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Boonton's 4540 Peak Power Meter delivers the outstanding performance needed for today's demanding radar and communication applications. By incorporating advanced technology from our flagship 4500B peak power analyzer, the smaller, economically priced 4540 outperforms higher priced competitors in many areas. It's fast update rate enables tuning high power amplifiers and processing large amounts of statistical data for CCDF measurements. Advanced trigger technology provides a rock solid view of fast rise time signals and the wide dynamic range allows measuring low duty cycle pulses. The 4540 power meter provides automatic settings for a large number of technologies including WCDMA, WiMAX, WLAN, Wi-Fi, LTE, and Radar.

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- Statistical analysis including CCDF
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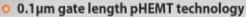
**Boonton** 



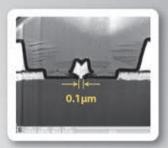


## New 0.1µm pHEMT Technology

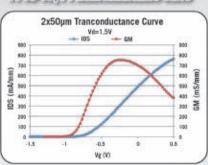
WIN is the world's largest and leading 6" GaAs foundry



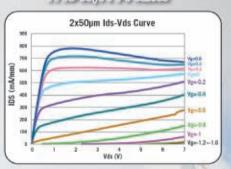
- 9V off-state breakdown voltage for power application
- Wafer thickness options of 50um (PP10-10) and 100um (PP10-11) available
- 860 mW/mm P<sub>sat</sub> at 29GHz with Vd=4V
- 400 mF/mm<sup>2</sup> capacitor for design flexibility



#### PP10-10, 11 Tranconductance Curve



#### PP10-10, 11 I-V Curves



#### Comparison of WIN's millimeter wave pHEMT technologies

	PP25-21	PP15-50/51	PP10=10/11
Gate length	0.25µm	0.15µm	0.1µm
Operating Frequency	Up to 20GHz	Up to 30 GHz	Up to 90GHz
Max Drain Bias	8V	6V	4V
Max Id (Vg=0.5V)	490 mA/mm	630 mA/mm	760 mA/mm
IDSS (Vg=OV)	340 mA/mm	470 mA/mm	520 mA/mm
Max Gm	410 mS/mm	460 mS/mm	725 mS/mm
Vto	-1.15 V	-1.35 V	-0.95 V
Von (Diode turn on)	0.8 V	0.8 V	0.9 V
BVGD	20V (18V min)	16V (14V min)	9V (8V min)
f <sub>T</sub>	65 GHz	90 GHz	130 GHz
f <sub>max</sub>	190 GHz	185 GHz	180 GHz
Power Density (2x75µm)	1100 mW/mm @ 8V, 10GHz	870 mW/mm @ 6V, 29GHz	860 mW/mm @4V, 29GHz (2x50μm)





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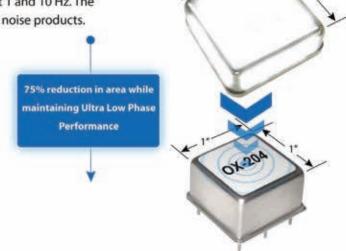
#### **Key Features**

- -135 dBc / Hz at 10 Hz offset
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- 10 MHz standard, other frequencies available
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  - 4 Watts during warm-up
  - 1.5 Watts during steady state
- Temperature Stability:
  - +/-10ppb at -20 to 70°C
  - +/-20ppb at -40 to 85°C

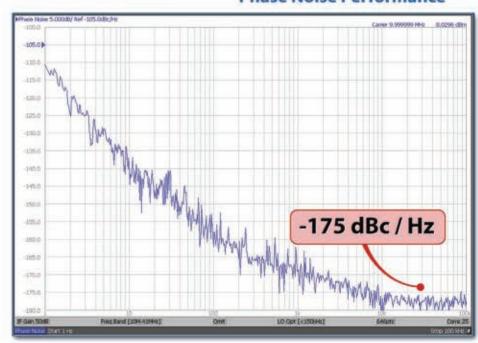
## **Applications**

- Radar
- Satellite Communications
- Military Communications
- **Test & Measurement Equipment**
- **DRO & Synthesizer references**





#### **Phase Noise Performance**



OCXO/EMXO

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VCSO VCXO Jitter Attenuation

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MSW2001-200	T-R Switch, TX Left	+V Only	MPD2T28125-700	400 to 4,000					
MSW2002-200	T-R Switch, TX Left	+V Only	MPD2T28125-700	2,000 to 6,000					
MSW2022-200	T-R Switch, TX Right	+V & -V	MPD2T5N200-702	2,000 to 6,000					
MSW2050-205	T-R Switch, TX Left	+V Only	MPD2T28125-700	20 to 1,000					
MSW2051-205	SW2051–205 T-R Switch, TX Left		MPD2T28125-700	400 to 4,000					
MSW2030-203	Symmetrical SP2T	+V Only	MPD2T28125-700	10 to 1,000					
MSW2031-203	Symmetrical SP2T	+V Only	MPD2T28125-700	400 to 4,000					
MSW2032-203	Symmetrical SP2T	+V Only	MPD2T28125-700	2,000 to 6,000					
MSW2040-204	Symmetrical SP2T	+V Only	MPD2T28125-700	50 to 1,000					
MSW2041-204	2041–204 Symmetrical SP2T		MPD2T28125-700	400 to 4,000					
MSW2060-206	Symmetrical SP2T	+V & -V	MPD2T5N200-702	10 to 1,000					
MSW2061-206	Symmetrical SP2T	+V & -V	MPD2T5N200-702	400 to 4,000					
MSW2062-206	Symmetrical SP2T	+V & -V	MPD2T5N200-702	2,000 to 6,000					
MSW3100-310	Symmetrical SP3T	+V Only	MPD3T28125-701	10 to 1,000					
MSW3101-310	Symmetrical SP3T	+V Only	MPD3T28125-701	400 to 4,000					
MSW3200-320	Symmetrical SP3T	+V & -V	MPD2T5N200-703	10 to 1,000					
MSW3201-320	MSW3201-320 Symmetrical SP3T		MPD2T5N200-703	400 to 4,000					

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SemiGen Inc.

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Describes the design and manufacture of a set of E- and W-Band MMIC power amplifiers based on six-inch 0.1 µm GaAs technology

## 184 Compact UHF Fifth Order Bandpass Filter Using Cascaded Triplet CRLH-ZORs

Boram Lee and Sungtek Kahng, University of Incheon Presents a bandpass filter made very compact by implementing the CRLH ZORs and their coupling and forming a CT to have a steep skirt for high frequency selectivity













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#### **Quarter Substrate Integrated Waveguide Resonator Applied to** Fractal-Shaped BPFs

Sheng Zhang, Tian-Jian Bian and Yao Zhai, China University of Mining and Technology; Wei Liu, Guang Yang and Fa-Lin Liu, University of Science and Technology of China

Presents a quarter substrate integrated waveguide (SIW) resonator and a fractalshaped defected structure used to design miniaturized SIW bandpass filters

#### PRODUCT FEATURES

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Agilent Technologies Inc.

Introduction to the new X-Series of signal generators that are available in analog and vector modulation models, from the pure and precise MXG to the costeffective EXG

## 218 Single Chip AGC Solutions for Communications

Hittite Microwave Corp.

Introduction to a new line of highly integrated analog AGC solutions that address many of the complex challenges of designing high performance AGC loops

### **226** Half Watt Driver Amplifier with Dynamically Adjustable Bias

Analog Devices

Development of a new 1/2 W RF driver amplifier that incorporates a dynamically adjustable biasing circuit with a wide operating temperature range

#### **230 Exploit the Radio Channel for Improved MIMO Performance**

EB (Elektrobit)

Introduction to the new EB Propsim® F32 radio channel emulator that meets the demanding design and verification challenges of today's and future wireless technologies

#### TECH BRIEFS

### **Wideband Synthesized Signal Generators**

Mini-Circuits

#### **Small Vector Reflectometer**

Copper Mountain Technologies

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Agilent in Aerospace/Defense

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**Besser Training Series - Mixers** 

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**Understanding Radio Channel: Part 2** 

5/23/12 at 12:00 PM ET Sponsored by: EB (Elektrobit)

RF and Microwave Heating

with COMSOL Multiphysics Sponsored by: COMSOL

5/24/12 at 2:00 PM ET

**Innovations in LTE** 

by: Agilent Technologies LTE Channel State Testing

5/31/12 at 1:00 PM ET



**March Survey** "Who's the better engineer?"

You [66 votes] (14%)

Your boss [15 votes] (3%)

The company "Guru" [16 votes] (3%)

The new PhD Hire [6 votes] (1%)

That "old guy" that left the company [372 votes] (78%)



#### Executive Interview

Janne Kolu, Vice President of Test Tools, EB (Elektrobit), explains the company's global reach, elaborates on the evolution of test systems in the wireless sector and discusses EB's latest product developments.

## White Papers

Statistical Analysis of Modern Communication Signals Bob Muro, Wireless Telecom Group

Redefining RF and Microwave Instrumentation Through Open Software and Modular Hardware Tutorial, National Instruments

Selecting Ferrite Circulators for Radar Applications Presented by: Richardson RFPD and Skyworks

Leverage Circuit-Envelope Simulation to Improve 4G PA Performance Dr. John M. Dunn, AWR Corp.

LO Harmonic Effects on TRF3705 Sideband Suppression Bill Wu and Russell Hoppenstein, Texas Instruments

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- . Options for Leakage Levels
  - -10 dBm
  - 5 dBm
  - 0 dBm
  - + 5 dBm
- . Removable connectors for circuit board assembly
- . Ideal for LNA Protection

MODEL	FREQ. RANGE (GHz)	NOMINAL <sup>2</sup> LEAKAGE LEVEL (dBm)	TYPICAL <sup>1</sup> LEAKAGE LEVEL (dBm)	TYPICAL 3 THRESHOLD LEVEL (dBm)	
LL00110-1 LL00110-2 LL00110-3 LL00110-4	0.01 - 1.0	-10 - 5 0 + 5		-11 - 6 - 1 +4	
LL0120-1 LL0120-2 LL0120-3 LL0120-4	0.1 - 2.0	-10 - 5 0 + 5	:	-11 - 6 - 1 + 4	
LL2018-1 LL2018-2 LL2018-3	2-18	•	-10 TO -5 - 5 TO 0 0 TO -5	-10 - 5 0	

#### Notes:

- 1. DC Supply required: +5V, 5mA Typ.
- 2. Typical and nominal leakage levels for input up to 1W CW.
- 3. Threshold level is the input power level when output power is 1dB compressed.

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Deadline: June 29, 2012 IEEE International Symposium on RF Integration Technology Deadline: August 6, 2012

#### **ONLINE: COMING SOON**

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#### JUNE

#### **JNC 2012**

JOINT NAVIGATION CONFERENCE

June 12–15, 2012 • Colorado Spring, CO www.jointnavigation.org

#### **RFIC 2012**

IEEE RADIO FREQUENCY INTEGRATED CIRCUITS SYMPOSIUM

June 17–19, 2012 • Montréal, Canada www.rfic2012.org

#### IMS 2012 IEEE MTT-S

International Microwave Symposium June 17–22, 2012 • Montréal, Canada

www.ims2012.org

#### MICROAPPS 2012

THE MICROWAVE APPLICATION SEMINARS

June 19–21, 2012 • Montréal, Canada http://ims2012.mtt.org/en/node/207

## **79**<sup>TH</sup> **ARFTG M**ICROWAVE **M**EASUREMENT **C**ONFERENCE

June 22, 2012 • Montréal, Canada www.arftg.org

#### JULY

2012 IEEE INTERNATIONAL SYMPOSIUM ON ANTENNAS AND PROPAGATION AND USNC-URSI NATIONAL RADIO SCIENCE MEETING

July 8–14, 2012 • Chicago, IL www.2012apsursi.org



#### **AUGUST**

#### **IEEE EMC 2012**

August 5–10, 2012 • Pittsburgh, PA http://2012emc.org

**AUVSI UNMANNED SYSTEMS N. AMERICA 2012** 

August 6–9, 2012 • Las Vegas, NV www.auvsishow.org

#### **SEPTEMBER**

#### MMS 2012

**12<sup>TH</sup> MEDITERRANEAN MICROWAVE SYMPOSIUM** September 2–5, 2012 • Istanbul, Turkey

www.mms2102.org

#### **ICUWB 2012**

IEEE INTERNATIONAL CONFERENCE ON ULTRA-WIDEBAND

September 17–20, 2012 • Syracuse, NY www.icuwb2012.org

#### **ION GNSS 2012**

September 17–21, 2012 • Nashville, TN www.ion.org



#### **OCTOBER**

## EuMW 2012

## MILCOM

#### COMSOL

8<sup>TH</sup> ANNUAL MULTIPHYSICS CONFERENCE

October 3–5, 2012 • Boston, MA www.comsol.com/conference2012/usa/

MICROWAVE UPDATE 2012

October 18–21, 2012 • Santa Clara, CA www.microwaveupdate.org

#### **AMTA 2012**

34<sup>TH</sup> ANNUAL SYMPOSIUM OF THE ANTENNA MEASUREMENT TECHNIQUES ASSOCIATION

October 21–26, 2012 • Bellevue, WA www.amta.org

#### **RADAR 2012**

INTERNATIONAL CONFERENCE ON RADAR

October 22–25, 2012 • Glasgow, UK www.radar2012.org

#### EuMW 2012

EUROPEAN MICROWAVE WEEK

October 28–November 2, 2012 Amsterdam, The Netherlands www.eumweek.com

#### MILCOM 2012

MILITARY COMMUNICATIONS CONFERENCE

October 29–November 1, 2012 • Orlando, FL www.milcom.org

#### 4G WORLD 2012

October 29–November 1, 2012 • Chicago, IL www.4gworld.com

#### NOVEMBER

#### **IME 2012**

**7<sup>TH</sup> INTERNATIONAL CONFERENCE AND EXHIBITION ON MICROWAVE AND ANTENNA** 

November 5–7, 2012 • Shanghai, China www.imwexpo.com

#### **ELECTRONICA 2012**

November 13–16, 2012 • Munich, Germany www.electronica.de

#### **DECEMBER**

#### **APMC 2012**

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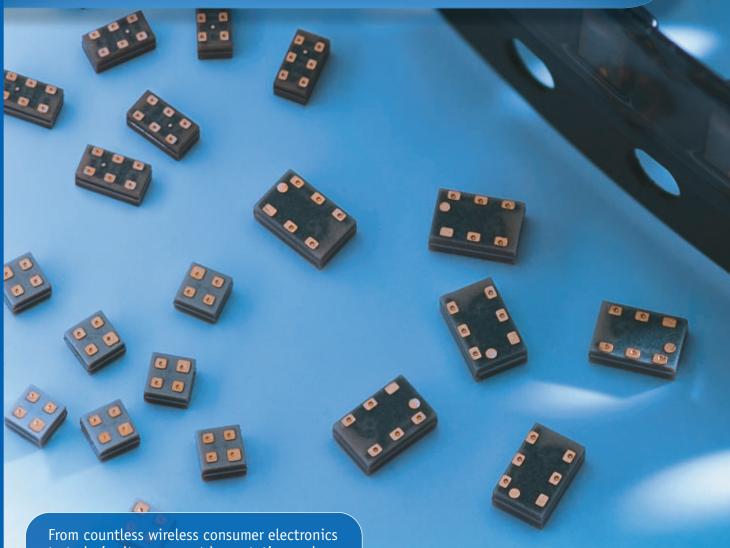
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# May We Have Your Attention Please...

n March 2013, Microwave Journal and its parent company Horizon House will launch La new conference and trade show focused on high frequency electronic design. Electronic Design Innovation Conference (EDI Con) will be held March 12-14 in Beijing, complementing the introduction of our new print magazine, Microwave Journal China and companion website microwavejournalchina.com. The event will be developed in collaboration with the companies that currently contribute to the Journal and operate in China. Our aim is to develop the premier communication channel for advancing microwave technology in this growing market through print, electronic media and a dedicated conference/ trade show.

At the Journal, we have been giving this project much thought and recognize this as an opportunity to design a different kind of program, albeit one that reflects the editorial focus of our magazine and the design community's needs. In its first year, EDI Con will be a two and a half day event with a technical program featuring the latest design techniques and technologies, workshops for advanced professional education and product training, business panels to discuss market trends and an exhibition of leading microwave companies.

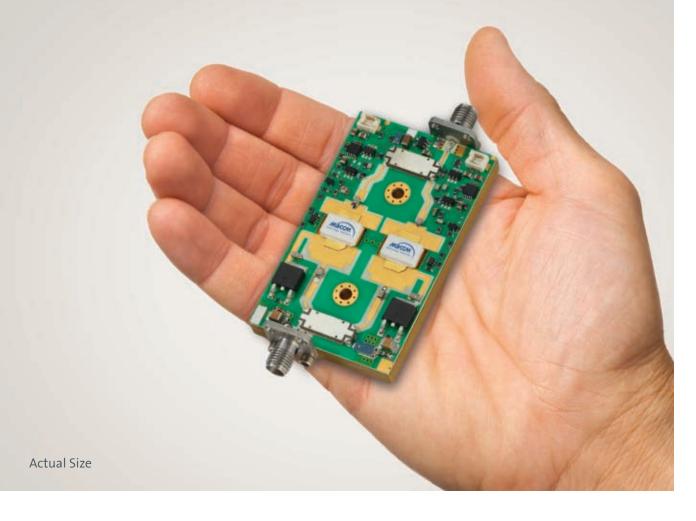
The technical program will be developed in partnership with industry and local academia with an emphasis on design trends and the needs of the industries we serve. Papers, workshops and tutorials will encompass all aspects of high frequency/high speed design from new semiconductor processes and circuit architecture, to the advanced miniaturization and integration of microwave components and subassemblies necessary for tomorrow's communication systems. Topics will include advanced materials and semiconductors, simulation and EM modeling, as well as testing at the component and system levels.

The Journal often presents microwave technology in the context of business and industry. EDI Con will offer a similar balance with keynote talks and panel sessions featuring high-level executives from both industry and government. Designing a conference from the ground up provides the perfect opportunity to apply lessons learned from our involvement in a variety of other events and the freedom to innovate. By announcing this initiative now, we are reaching out to potential partners in this venture and we look forward to your feedback when we meet face to face in Montréal. We hope you participate. After all, there is no business like show business. And it all starts in Beijing, March 2013.

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DAVID VYE Microwave Journal Editor

# POWER IN THE PALM OF YOUR HAND



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# Canada

# Oh Canada!



arlier this year, I participated in an industry focus group where we were asked the following question: "What is the number one opportunity for microwave technology and who is in the best position to capitalize on it?" My knee jerk response was to offer a short list of hot markets, including 4G, mobile internet, M2M, aerospace and defense, etc. In contrast, the technicallyinclined members of the group saw opportunity from a completely different perspective. For them, opportunity was the chance to utilize spectrum more efficiently or to get more functionality into a smaller component.

It was an eye-opening moment for me, the realization that engineers view problems as opportunities. Besides being a great personality trait, it is a point of view that has widespread ramifications. While the promise of financial reward from future markets may fund R&D, it is technical advancement that creates markets and it is those who see problems as opportunities that lead the way. Rethinking the question, I now side with those who say the greatest opportunity in our field belongs to whoever can pack the most RF/microwave functionality into the smallest footprint (and I'll add "lowest cost" to

the wish list). Miniaturization and integration have always been the leading technical goals for our industry and the International Microwave Symposium (IMS) is a great opportunity to assess where we are in that quest.

IMS has two major components, namely the technical conferences and the exhibition. In terms of size and quality, the technical program is unparalleled in its focus on microwave technology. How good are the technical papers presented at IMS? In our November 2011 cover story, the Journal reported on the industry's leading innovations. Our list of the top ten innovations of 2011 was compiled largely by cross-referencing three sources - twelve months of Microwave Journal editorial and the technical programs from IMS and European Microwave Week. If it is new and significant, it will be in the IMS technical program. Overviews of this year's technical programs are featured in this month's welcome messages from the IMS, RFIC and ARFTG chairs.

Of course the other component to IMS is the exhibition. This spring, many of you will be attending your share of industry-related trade shows or preparing new products to be introduced at these events. Some shows will be

focused around a specific market/industry such as Mobile World Congress (see MWJ International Editor, Richard Mumford's show wrap-up in this issue, pg. 106) or CTIA Wireless. These are large events (40,000+ attendees) in which RF/microwave technology plays a small but critical part in the overall event eco-system. But the exhibition at IMS is all about our technology – the latest microwave components, subsystems, test solutions and software products.

For a preview of what will be on display, check out this issue's new IMS Product Showcase, pg. 250. This year, we are trying out a bold experiment to enhance the Microwave Journal user experience. Showing a bias to those folks that will be at the exhibition, we have organized products by their location on the exhibition floor rather than by product category. So when an attendee is standing in aisle 1500 for example, Microwave Journal will tell them what new products are nearby. The full exhibitor list with booth number (companies whose advertisements appear in this issue are in red) and the show floor map

(Continued on pg. 30)

**DAVID VYE**Microwave Journal *Editor* 

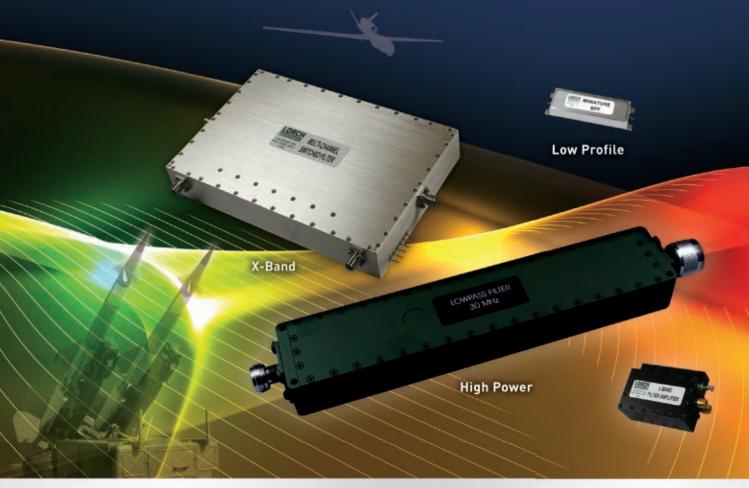
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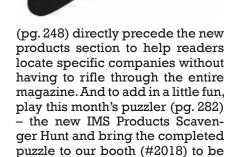




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As an event that travels to different locations each year, IMS is also about its host city. And this year, the MTT-S is celebrating its 60th year by holding the symposium outside the U.S., truly living up to its "International" title. Montréal is a beautiful city, within driving range from many East Coast cities and hopefully a powerful draw for the international audience that the society is aiming to attract. The Journal celebrates this location with our latest graphic novel, "Montréal Road Trip 2012"a salute to those of you pulling late hours to get new products ready in time for the event.

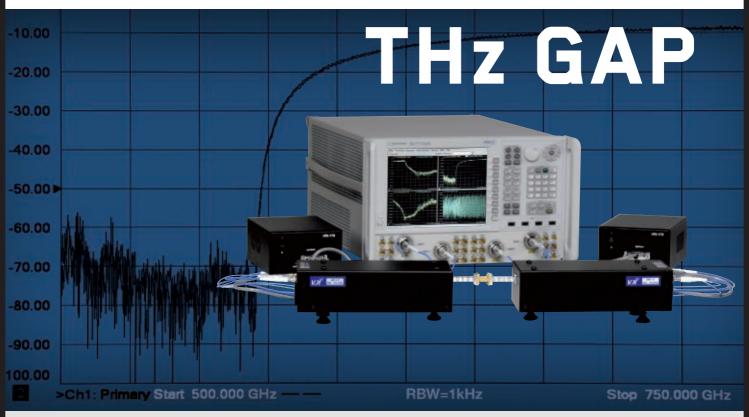
Also, this month's cover story pays tribute to the region's technical roots with a look at the rise and fall of former Canadian telecommunication giant, Nortel. This is a fascinating story of the vision and innovation that made this company a powerhouse during the dot com bubble and helped establish the Montréal-Ottawa-Toronto technology belt as world class.

Since the days when Ted Saad served as this magazine's first editor and was instrumental in creating the MTT-S, our two organizations have enjoyed a close and personal relationship. As an IMS media partner, it is a pleasure to support the event through our extended coverage and we thank the organizers for the opportunity to interact with attendees through the Cyber Café, the Device Characterization & Design Expert Panel at MicroApps and Strategy Analytics' "RF Market Opportunities for GaN" Panel. Congratulations to the MTT-S on turning 60 and we will see all of you problem solvers looking for opportunities in the Great White North.

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Dynamic Range (BW=10Hz,dB,typ)	120	120	120	120	120	110	100	100	60	
Dynamic Range (BW=10Hz,dB,min)	100	100	90	90	90	90	80	80	40	
Magnitude Stability (±dB)	0.15	0.15	0.15	0.25	0.25	0.3	0.5	0.8	1	
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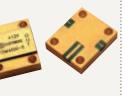


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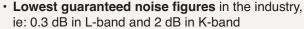






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he birthplace of the world's first smartphone is a one hour drive west from this year's IMS at the Palais des Congrès de Montréal. In 1998, ten years before Apple unleashed its iPhone or Research in Motion (RIM) of Waterloo, Ontario hit it big with the BlackBerry, a small group of engineers, industrial designers and psychologists at Nortel's Corporate Design Group in Ottawa developed the "Orbitor." This handheld device could transform into a pager, voice mailbox, fax machine or wireless phone with the simple touch of a finger or stylus. The company's R&D group had 80 finished units ready for market with service delivery trials set to begin with one of Europe's largest cell phone operators. Nortel had leveraged its joint venture in GSM with French company Matra (1992) and four years of internal development to produce a potential game-changing product. This level of market-leading innovation was not a fluke for Nortel's massive research center and the city known as Silicon Valley north.

Established in 1961, the epicenter of Nortel Networks' research and development was known as the Carling Campus. With a man-made lake and 11 glass and steel buildings totaling over 2 million square feet connected by underground tunnels, the campus was originally built to house 9000 workers. In addition to the 6700 employees engaged in advanced research and product development, the company employed nearly 2300 employees dedicated to manufacturing, marketing, operations and services. Less than a mile from the Carling site, Nortel's Technology Supply and Components organization operated its own 500,000 square foot Corkstown facility, home to Nortel Semiconductors, which designed and manufactured custom microchips and application-specific integrated circuits (ASIC); and Nortel Microwave Modules, which manufactured RF, wireless and transmission multi-chip modules.

In 2001 at the company's height, Nortel had 16,000 employees working in Ottawa with 12,000 of them in R&D. Researchers were working in all areas of hardware,

#### DAVID VYE

Microwave Journal Editor

# RF & MICROWAVE FILTERS

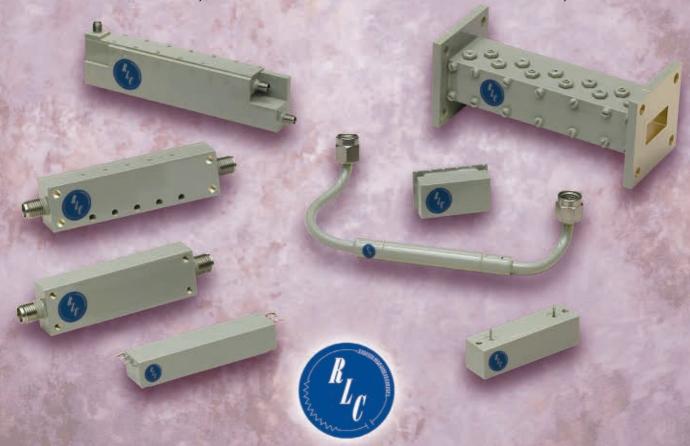
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# Canada



software and semiconductor technology among multiple labs, including the Physical Design Integration Group, which focused on systems packaging and product integrity at the nearby Kanata complex. Ten years later, the nearly empty campus would be sold to the Public Works and Government Services Canada for a cash purchase price of CDN\$ 208 million. The fall of Nortel marks a dark period in the long history of a vibrant and innovative Canadian-based telecommunications industry. Over 6000 patents, the intellectual output of this colossal R&D workforce, would be licensed to a consortium of foreign telecom OEMs for CDN\$ 4.5 billion and the Orbitor would remain an obscure footnote in the development of mobile technology.

#### THE BIRTH OF BELL CANADA



Montréal lies at the eastern tip of Canada's Montréal-Ottawa-Toronto technology corridor and was home to the earliest manufactur-

ing within the telecommunication sector. The industry got its start at the western tip, in the outskirts of Toronto in the town of Brantford, Ontario where Alexander Graham Bell first conceived the telephone in 1874. Bell's concept of transmitting speech electrically came into sharper focus in Boston where he created his "harmonic telegraph," along with his collaborator, Thomas Watson. Working in the transmitter room on June 2, 1875, Watson unintentionally produced and transmitted a twanging sound while trying to free a reed that had been too tightly wound to the pole of its electromagnet. Bell heard the sound from the receiving room and realized the complex overtones and timbre was similar to the human voice. Inspired by this accident, Bell raced to perfect his telephone while also writing up specifications to be filed with the United States Patent Office.

On February 14, 1876, Alexander Graham Bell's telephone patent application entitled "Improve-

ment in Telegraphy" was filed by his attorney; just a few hours before the attorney for a Western Electric inventor named Elisha Grav filed a caveat for a telephone entitled "Transmitting Sounds Telegraphically." A patent caveat was a type of preliminary application for a patent that gave an inventor an additional ninety days grace to file a regular patent application. The caveat would prevent anyone else that filed an application on the same or similar invention from having their application processed for ninety days. Alexander Graham Bell was the fifth entry of that day, while Elisha Gray was 39th. Therefore on March 7, 1876, rather than honor Gray's caveat, Bell was awarded the first patent for a telephone - US Patent No. 174,465. Controversy persists to this day over the filing of these patents and the true ownership of the invention. Three days after being awarded the patent, Bell built and successfully tested Gray's liquid transmitter design, famously transmitting his "Mr. Watson, come here, I want to see you" message. On September 12, 1878, lengthy patent litigation involving the Bell Telephone Co. against Western Union Telegraph Co. and Elisha Gray began.

The Bell Telephone Co., was organized in Boston in 1877 by Bell's father-in-law Gardiner Greene Hubbard, and was started for the purpose of holding "potentially valuable patents," principally Bell's master telephone patent. The company subsequently merged with others (including Hubbard's National Bell Telephone Co.) to form the American Bell Telephone Co., which would later evolve into AT&T under the direction of Thomas Vail. Bell gave 75 percent of the Canadian patent rights to his father who served on the board of directors for Bell Telephone of Canada, incorporated in 1880. Bell Canada would operate telephone exchanges throughout Canada and manufacture telephones and associated equipment.



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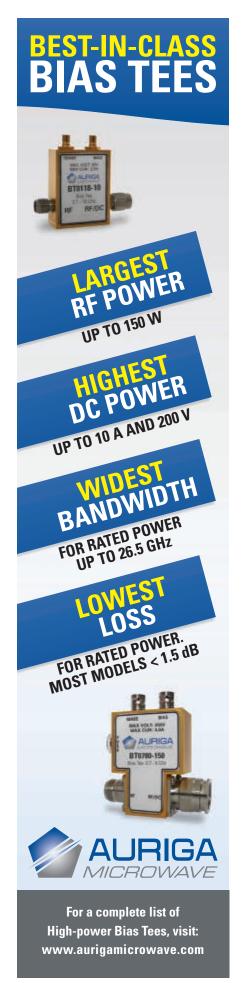
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## Canada Montréal da



#### NORTHERN ELECTRIC IS CREATED



In 1881, a former New England sea captain named Charles Fleetford Sise unified all of the Canadian telephone networks under

the aegis of Bell Telephone of Canada. He then began developing long-distance networks between cities. When the operator of the world's first telephone manufacturing plant died of tuberculosis, Sise lost his domestic supply of telephone equipment. Without an alternative Canadian supplier he would lose the Canadian patent rights. Had it not been for this law and his inability to find an alternative supplier, Sise may not have been pressured to start his own manufacturing plant and subsequent R&D labs.

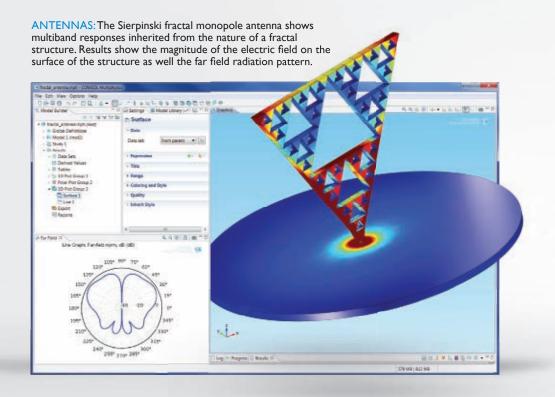
After consulting with Theodore Vail, president of the National Bell Telephone Co., a major shareholder in the Canadian telephone business and the man often credited with creating the nationwide AT&T network, Sise hired an experienced foreman from National Bell's Boston plant and rented two floors of a building in Montréal for manufacturing. The mechanical division of The Bell Telephone Co. of Canada began in 1882 with the arrival of Brown and the rental of those two floors. In addition to phones, the department would start manufacturing its first switchboard, a 50 line Standard Magneto Switchboard. The popularity of the telephone led to yearly growth and an expansion to 50 employees by 1888, transforming into a separate manufacturing branch with 200 employees and a new factory under construction by 1890.

Shortly, the production capacity outpaced demand for phones and the branch faced closure unless it could manufacture other products. In 1895, Bell Canada spun off its manufacturing arm to expand by building phones for other companies as well as other devices such as police and fire department call boxes. This new company was incorporated as Northern Electric

and Manufacturing Co. Ltd.

By 1899, Bell Telephone of Canada purchased the Barrie and Johnson Wire and Cable company, which it had renamed the Imperial Wire and Cable Co. Northern Electric Co. amalgamated with Imperial in 1914 and moved to a new factory located at Shearer Street in Montréal. This facility would be the company's primary manufacturing center until the mid-1950s. In between that time, Northern Electric would grow alongside the technology that marked the first half of the twentieth century, developing a one-wire telegraphic switchboard for military service known as the portable commutator in WWI; in 1922, Northern developed the first Canadian vacuum tube - a \$5 "Peanut" tube that was the smallest made, requiring only one-tenth of an amp, which was used on repeater apparatus for long-distance lines. The company also grew with the production of a large commercial grade radio system in 1923 and general use consumer radios in 1926.

With Canada pulled into WWII, the government froze development of non-military products in 1941, but placed orders for \$40 million worth of military supplies. This represented 2.5 times the company's sales from 1939, leading to an expansion from 5000 to 8000 employees working around the clock to meet production demand and develop new technologies. Northern Electric supplied electrical equipment for Royal Canadian Navy Destroyers and produced a two-way wireless set for telephone communications between tanks and other military vehicles operated by Canadian, British and Russian armed forces. The company was also developing expertise in new technologies such as radar and microwaves, delivering 19,000 magnetron tubes for radar. This expertise would serve the company well after the war in its development of Canada's first microwave relay long-distance telephone and television systems.



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#### CUTTING THE CORD WITH BELL LABS

O I

Before Bell came along, Western Electric was the principal manufacturer for Western Union, the telegraph company. In 1882

Western Electric joined the Bell System (Bell purchased a controlling interest in its stock) and subsequently the company manufactured in every country with significant telephone systems. Bell's subsequent acquisition of Western Electric was crucial in the establishment of a nationwide phone system, a system characterized by its early, primary emphasis on the production and distribution of hardware. Western Electric owned 44 percent of Northern Electric, the rest was owned by Bell of Canada. For the first fifty years of the company's existence, Northern Electric essentially manufactured equipment based on designs and processes licensed from Western Electric.

In 1949, the Department of Justice sought the separation of Western Electric (manufacturing) from AT&T (service). As a consequence of this antitrust case, AT&T was ordered to divest all of its nontelephone activities, except those involving national defense. The 1956 consent decree also called for Western Electric to relinquish its 40 percent interest in Northern Electric of Canada, the last vestige of its international operations. Under the decree, Western Electric terminated its patent and licensing relationship with Northern Electric.

Cut off from its major technol-

ogy wellsprings, Northern would either have to license technologies from others in the Canadian market or create its own technologies to compete in world markets. Choosing the latter, Northern Electric began to achieve technical independence in 1957 by creating its own research and development facilities in Belleville, and, in 1959, established Northern Electric Research and Development Laboratories in Ottawa, Ontario. At the same time, Bell Canada began stepping up its own development activities.

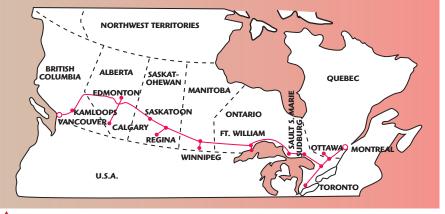
#### NORTHERN DEVELOPS TRANS-CANADA SKYWAY



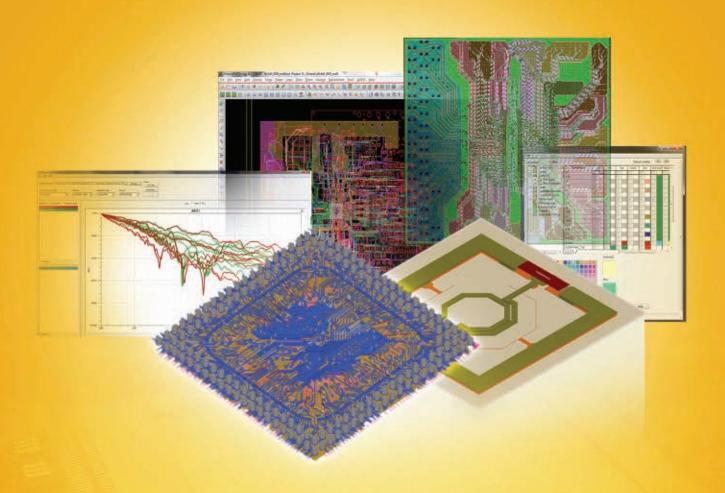
In 1958, Northern built the equipment for the Trans-Canada Skyway, the world's longest microwave transmission network spanning

over 6275 km at a cost of \$50 million (\$375 million in 2012 dollars). The system was implemented under Bell Canada president Thomas Eadie as an all-Canadian microwave network for transporting telephone conversations, teletype messages and television signals. This microwave-relay used 139 line-of-sight repeater stations spaced at approximately 25 mile intervals, to make a connection from Sydney, Nova Scotia to Victoria, British Columbia. The system allowed a microwave signal to travel from one coast to the other in just one-fiftieth of a second.

The towers ranged from nine meters high to over 100 meters high in northern Ontario (see *Fig-*



▲ Fig. 1 Route of the Trans-Canada Skyway microwave system.



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ure 1). The 10 or 12 foot diameter parabolic antennas were fed by rectangular waveguide with ferrite isolators and circulators enabling two transmitters and two receivers to be connected to one dish, providing two separate message channels through the repeater in each direction. In the interest of providing greater isolation, the received signal was re-transmit-

ted 252 MHz above or below the received frequency. The systems used eight such frequencies ranging from 5.974 to 6.404 GHz with 118 MHz spacing between two channels over the same path in the same direction. Each received carrier, at a level of approximately 1 micro watt, together with the local oscillator output, entered a balanced crystal mixer pre-amp

whose 70 MHz output was pre-amplified to 0.09 V rms.

#### A NEW EMPHASIS ON R&D



Chief executive Cy Peachey joined the company in the 1920s and was instrumental in establishing the company's ethos of internal re-

search and development. When Northern Electric was deprived of its links to Western Electric after the U.S. antitrust action, Peachey declared, "We know how to do it. We've got good engineers and we're going to build our research and development organization and we're all going to be pretty proud of it." As a major force at the company until the 1960s, he helped establish research labs in Belleville, Ontario (1957) and two years later in Ottawa, which started out with 42 engineers but grew to 800 people within five years. The lab was responsible for developing a growing list of successful products such as the very modern Contempra telephone (see Figure 2) featuring the first dial-in-hand design. This product sold into 3.4 million homes and was put on display at New York's Museum of Modern Art.

On the technology side, the R&D labs developed the SA-1 community dial office (CDO), a small Class 5 Crossbar for local switching used in telephone exchanges in rural areas. Rural communities represented a sizable portion of Canada's sparse population and provided a good market niche for Northern to capitalize on while serving the unique communication needs of its customers. Freedom from AT&T allowed local engineers to pursue their own so-



Fig. 2 Northern Electric's Contempra phone, the first dial-in-hand design.



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lutions for a market with different needs than those of its southern neighbors.

Communications for rural living provided an opportunity in the SATCOM business in the 1960s. When the Canadian Parliament decided to establish a domestic communications satellite network called Telesat Canada, Northern played a key technical role. As a

prime subcontractor for Hughes Aircraft, Northern developed the satellite electronics and antenna equipment. The Anik A satellite system, which cost \$90 million at the time, made Canada the first country to utilize synchronous satellite for domestic communication purposes. A contract for three satellites to operate in the 6/4 GHz range was awarded to Hughes

Aircraft, with the participation of Northern Electric and Spar Aerospace (another Canadian company). Each satellite provided twelve high-capacity microwave channels for color television or as many as 960 one-way telephone calls. Of the thirty-seven ground stations built, twenty-four were equipped with receive only capability to provide live television programming to isolated Northern communities. This reduced the cost of the ground stations to \$150,000 each from oneto two-million dollars for units capable of carrying radio, television and two-way voice.

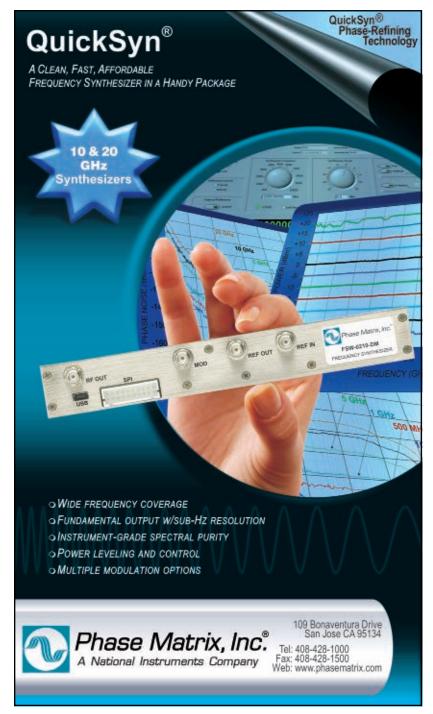




In September of 1969, under the direction of a young Bell Canada engineer named R. Charles Terreault, Northern Electric

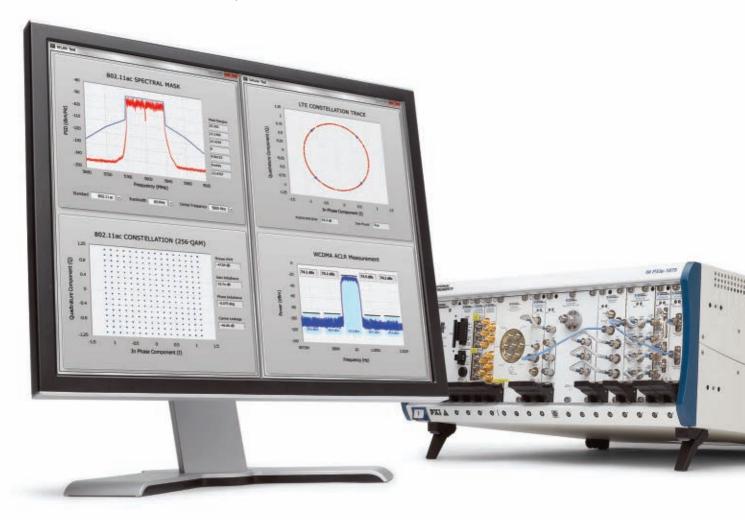
set out to create a twenty-year plan for developing a telecommunications network. Terreault assembled the twenty-person team that produced a monumental twelve-volume Long Term Network Evolution Study, drawing upon the latest developments in microelectronics. The plan forecast the total digitization of the network up to the point of ISDN then called Multiple-Use Selective Routing. Everything was planned decentralization of for, from switching toward the user to an orientation toward broadband switching (for video). The cornerstone of Terreault's plan was the introduction of a complete line of digital switches by the late 1970s and early 1980s.

When Bell Labs put its first digital transmission system, the T-1, into service in 1965, Terreault realized that the digitization trend was irreversible, not only in transmission but in switching. In 1971, Bell Canada and Northern Electric followed the U.S. by deploying their own hybrid system switch, the SP-1 – representing the first major technological achievement in the modern history of Canadian telecommunications. The small switch



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was ideal for rural independent operating companies and the \$60 million dollar R&D investment was a great success, helping Northern establish a U.S. market.

Terreault symbolized the new generation of Canadian researchers who had emerged since the split with Western Electric and Bell Labs. His Digital World team members were ready to pioneer the digital revolution in Canada and the global market, but he had to convince Bell Canada's senior management in the investment. The challenges were technological, organizational and economical. In 1971, Bell Canada and Northern Electric launched a joint venture Bell-Northern Research

(BNR) and the new-to-market SP-1 hybrid switch was just beginning to pay off its investment. There was internal resistance to undertake a new technical direction so quickly. When Terreault performed a series of impact studies on a five years status quo, all indicators showed that a rapid transition to fully digital switching would be profitable for the carrier.

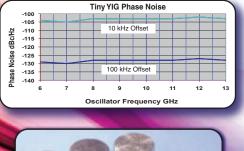
While many company executives agreed with the conclusions of the Long Term Network Evolution Study, they were skeptical about the pace of the transition to the digitalization world. Ultimately, Terreault's long-term plan was accepted and in 1972, Bell, Northern and BNR undertook a joint brainstorming session on digital switching that resulted in the definition of three essential elements: a private branch exchange (PBX), a lowcapacity public switch, and a high-capacity public switch.

By late 1972, Northern Electric released its first electronic switch. the SG-1 also known as PULSE PBX. Within three years, the company had sold 6000 units. In 1973, the engineers squeezed a translation coder-decoder (CODEC) unit onto a single integrated circuit, making it cost effective to convert between analog and digital and serve each telephone line with its own CODEC. This technical achievement was to be the key to all digital-switch programs and allowed Northern's first completely digital product, the SL-1 PBX with the capability to serve organizations with up to 7600 inside lines. Years ahead of any competition, the success of the SL-1 led the company to extend its digital technology to the telephone central office switch. Thus, BNR developed the Digital Multiplex System (DMS-10) for small central offices and the DMS-100, a full-featured, local/toll digital switch with support for 100,000 lines two years

Rapid growth in the United States became a model for further expansion in the Caribbean, Europe and the Pacific Rim. In Japan, the DMS-

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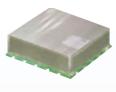


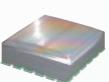


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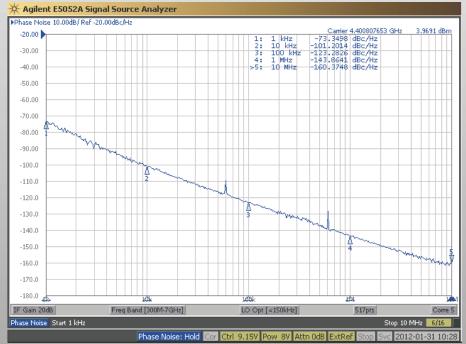


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10 allowed Northern to become the first non-Japanese supplier to Nippon Telegraph and Telephone, and opened markets in China and Eastern Europe. Because of an existing U.S. appliance maker called Northern Electric, the company renamed itself as Northern Telecom in 1976 and restructured its international subsidiaries under one corporate umbrella.

#### NORTHERN TELECOM ENTERS THE WIRELESS MARKET

0

Northern Telecom was part of the wireless revolution from the earliest days of cellular. In 1982, Northern Telecom and General Elec-

tric announced plans to develop, build and market cellular mobile communication systems based on switching provided by the DMS-100 and radio equipment from GE. That same year, AT&T was forced to spin off its Bell companies under pressure from the U.S. government, opening up the U.S. switching market to competition. As the second largest supplier of telecommunications equipment in North America, Northern Telecom was looking at a U.S. switching business worth \$320 billion a year.

The chief executive through this period of growth was John Roth. Roth was instrumental in establishing Northern Telecom's wireless business. Joining the company in 1969 as a design engineer, he was named COO in 1995 and then president in February 1997. Under his leadership, the R & D budget was bolstered to nearly 15 percent of revenue, which amounted to US\$ 1.58 billion in 1995. As the digital switching market matured, much of the research dollars went into new specialized areas and parallel restructuring of the company into four separate businesses. The first business was Northern's traditional switching operations that served old-line phone companies; one unit focused on broadband networks serving cable companies and the upstart long-distance companies created by the AT&T break-up; one specialized in enterprise networking serving large organizations including corporations and government departments - using internal communications networks; and one concentrating on wireless networks, which mainly served the rapidly expanding cellular telephone firms.

Roth wasted no time in mapping out the next step in the evolution of Northern Telecom, betting the company's future on the Internet. Roth saw that networks were going to migrate from telephone-based to Internet-based. He wanted Northern Telecom to be at the center of this build up of the Internet into a technology as reliable and accessible as the telephone. Needing to move quickly to beat



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# Canada Canada



out the competition, Roth turned largely to acquisitions rather than relying solely on in-house R&D efforts. The company's soaring stock facilitated the completion of stock-swap acquisitions.

Four major acquisitions were completed in 1998, including Winnipeg-based Broadband Networks Inc., a designer and manufacturer of broadband wireless communications networks (purchased for US\$ 593 million); Chelmsford, Massachusetts-based Aptis Communications Inc., a start-up firm that concentrated on remote-access data networking (US\$ 290 million); and Kanata, Ontario-based Cambrian Systems Corp., maker of an innovative technology to speed up Internet traffic (US\$ 300 million). These purchases were dwarfed, however, by the US\$ 9.1 billion stock-swap for California-based Bay Networks Inc. Bay Networks, the third largest maker of products linking computers to the Internet. served the corporate market with a host of data networking products and services that meshed well with Northern Telecom's existing corporate operations. The addition of Bay provided Northern with the ability to offer corporate customers integrated networks for sending voice, video and data over the Internet. With the company focusing increasingly on networking, Northern Telecom was renamed Nortel Networks Corp. in April 1999.

By the fall of 2000, Nortel Networks' market capitalization hit US\$ 240 billion, a six-fold increase since Roth had taken over as CEO. Roth planned to continue the breathtaking acquisition pace, vowing to spend ten percent of the company's market cap each year to purchase the new technology it would need to keep pace with the other heavyweights of networking, most notably Cisco Systems Inc., Ericsson and Lucent Technologies Inc. Nortel's emphasis on new technology was demonstrated by its generating 60 percent of its revenues from products less than 18 months old. The company had a clear focus on optical technology for many years. In 1966, researchers at BNR published the first paper considering the possibility of using glass fibers to carry information. By 1989, Nortel became the first telecom supplier to announce a complete family of SONET-standard fiber optic products. By 2000, Nortel was working to establish a more significance presence in the undersea-fiber business while gaining a reputation as a leader in the area of wireless Internet technologies.

#### THE DOWNFALL



Nortel once accounted for over a third of the value of the entire Canadian Stock Exchange, now known as the S&P/TSX Composite In-

dex. It became a giant through the surge in Internet demand in the latter half of the 1990s. That growth was also leveraged by the company's ambitious strategy of acquiring smaller companies to help it meet that demand. Nortel's reputation as a market heavyweight derived from its influence on the TSE 300 Composite Index. Unlike the Dow Jones, which is a priceweighted average of 30 stocks, the TSE 300 and the S&P/TSX Composite are float-weighted indices. which take into account the number of shares available, as well as the company's share price. So Nortel, which used to have 3.8 billion shares outstanding, wielded an enormous amount of influence.

The higher Nortel's share price went, the greater its weight in the index and the more the TSE 300 Composite Index rose. In 1999, the TSE 300 Composite Index rose by almost 30 percent, compared to the Dow's 25 percent rise. Without Nortel and BCE, the TSE 298 was up only 6.5 percent. The "Nortel effect" made it virtually impossible for investors or the manager of a diversified Canadian equity mutual fund to outperform an index that had a huge exposure to a stock that was doing so well. On the flip side, when Nortel's stock falls, so does the index, which is what happened on October 25, 2000. Company CEO, John Roth



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# Canada da



issued the first in a long series of sales warnings and the stock fell from \$96 to \$71 and the TSE 300 plunged 840 points in one day.

Throughout 2001, with its sales steadily collapsing, Nortel issued a stream of revenue and profit warnings and began a series of sweeping layoffs, cutting its 90,000-strong workforce by more than half. By the end of the year, the stock went from \$46 to under \$12. A continued sales slump and a downgrade of its longterm debt to "junk" status knocked the stock price down to 69 cents by October - less than 1 percent of where it had been just two years earlier and facing delisting from the New York Stock Exchange. The company that was once Canada's biggest now held the 46th spot and had a weighting in the S&P/TSX Composite Index of less than one percent.

Job cuts that brought the workforce down to 35,000 employees started to pay off on the bottom line by the spring of 2003. In April, the company reported its first quarterly profit in three years. Technology companies began buying equipment again and Nortel landed several high-profile billion-dollar contracts.

But just as Nortel's stock was recovering, the company announced that an accounting review had turned up "irregularities" and it would have to restate its finances back to 2000. In March 2004, two senior finance executives were put on leave and then fired the following month along with CEO Frank Dunn after Nortel revealed that its 2003 profit would be slashed in half. As regulators began investigating, the company cut another 3250 jobs. In May of 2005, after Nortel finally reported its 2003 and 2004 financial results, it was clear that the company was facing only modest revenue growth and Nortel's management was facing an increasingly competitive marketplace. The shares slipped to \$3 - their lowest point in more than two years.

Nortel paid out US\$ 575 million and 629 million common shares in 2006 to settle a class-action lawsuit that accused the company of misleading investors about the health of the company. On December 1, 2006, Nortel went ahead with the stock consolidation it had planned but never implemented back in 2002. It chopped the number of shares by 90 percent — a move that boosted its stock price 10-fold to the \$24 range. In February, 2007, Nortel announced its plans to reduce its workforce by 2000 employees, and to transfer an additional 1000 jobs to lower-cost job sites.

The Securities and Exchange Commission filed civil fraud charges against Nortel for accounting fraud from 2000 to 2003 to close gaps between its true performance, its internal targets and Wall Street expectations. Nortel settled the case, paying \$35 million. By February 2008, the stock was back below \$10 (\$1 on a preconsolidation basis) as losses grew and sales fell. By March, the stock had hit an all-time low. In late 2005, the company tried to engineer a turnaround. Mike Zafirovski, a former president and COO of Motorola took over as president after Nortel paid Motorola \$11.5 million to release him from his non-compete agreement. John Roese was brought in to help correct many years of neglect in R&D. Constant retrenchment at Nortel had left the fabled BNR legacy in tatters. Three years of painful rebuilding had given the company a growing financial safety margin, though only marginal profits, to start behaving like a contender again. In August of 2008, Nortel Networks announced it was buying Novera Optics and three other small companies, the first significant acquisitions in years. The price was modest, less than \$33 million, but it was the strongest signal that Nortel believed it was finally turning the corner and could compete for promising startups with Cisco Systems, where several of the company's newest executives had formerly worked.

But several failed business decisions and the freezing of global credit would thwart this turn around. On Roese's watch, Nortel sold promising but profitless

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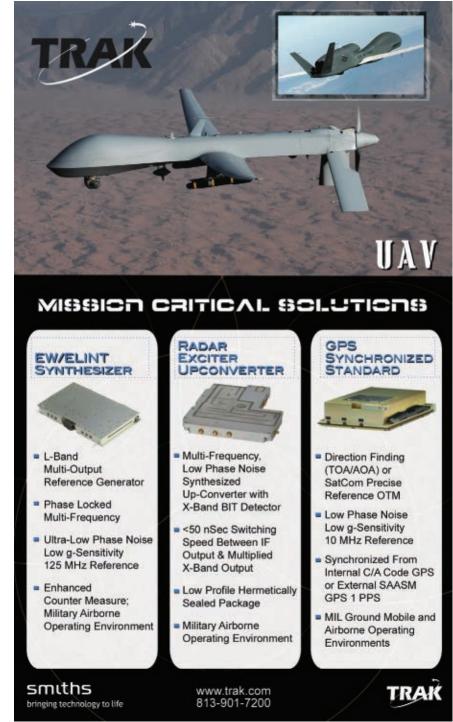
wireless equipment to Alcatel just as older generations of the same gear suddenly found big markets in emerging economies. Nortel had pulled out of India in the face of mounting losses, just as the market opportunity exploded, forcing the company to overhaul aging gear to generate some sales. And then the global financial crisis hit and the recession compounded

Nortel's financial challenges and directly impacted its ability to recover. In 2008, despite winning a contract from China Telecom for advanced wireless gear in seven provinces, the company had trouble financing the deal before it would start generating revenues sometime in the following year. During its reporting of third quarter 2008 results, Nortel announced

it would restructure into three vertically-integrated business units: Enterprise, Carrier Networks and Metro Ethernet Networks, this last entity had been put up for sale the previous month. The company, whose name had long been synonymous with optical networking gear, was selling off its Metro Ethernet Networks (optical and 40G) business to shore up the rest of the company and focus on 4G and related technologies. As part of the decentralization of the organization, four executive positions were eliminated including Roese. The company was in a death spiral.

In January 2009, Nortel Networks filed for creditor protection. The company reached this point after multiple management regimes had failed to remake the company after the telecom bubble burst. The company's demise was gradual but steady. The final phase in the Nortel saga was the pre-announced 3008 earnings (quiding down expectations), the sale of its Metro Ethernet Networks (MEN) division, and the latest reorganization. The announcement followed numerous incremental divestitures and shutdowns of specific businesses and product lines (for example, broadband access and the UMTS and WiMAX RAN segments) in an attempt to focus and differentiate while cutting costs.

Nortel hoped that by filing with a cash reserve of \$2.6 billion, the company would re-emerge as a leaner version of its former self in the future. Nortel's mobile infrastructure business was now solely focused on Long Term Evolution/ System Architecture evolution LTE/SAE using scarce product development dollars to fund another promising technology that North American phone companies wanted to support iPhones and other future devices capable of handling video and huge files. Nortel was also working hard to develop a strong LTE/SAE ecosystem including LG Electronics, LG Nortel and other partners, doing its best to demonstrate capabilities through trials with Verizon and T-Mobile Germany and hoping for



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some commercial launches within the vear.

But the bankruptcy filing was easily exploited by competitors who reminded customers that Nortel could no longer give assurances of continued development of any specific products and used the filing as a chance to reshuffle the supplier landscape to their benefit. After repeated restructuring,

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a shaky immediate financial outlook, shrinking market share, tight public credit markets and cautious investors, the cards were stacked against any such comeback.

#### THE SELL-OFF



Two and a half years after filing for bankruptcy protection, Nortel threw in the towel, announcing that a

consortium of six different companies had won the rights to its 6000 patents in a July 2011 auction. The list of winners included Apple, EMC, Ericsson, Microsoft, RIM and Sony. Not among the winners were Google, which placed the initial \$900 million stalking horse bid, and Intel. According to Nortel, the patents won a total of \$4.5 billion from the six companies involved. RIM indicated that it spent \$770 million in the auction, while Ericsson said it paid \$340 million. The other companies involved did not share the dollar value of their bids. The 6000 patents pertained to wireless technology, LTE 4G, data networking, voice technologies, and more. The auction was one of the final steps in Nortel's dissolution following bankruptcy. The proceeds will go to paying back Nortel's creditors.

#### THE AFTERMATH



In writing this article, I was in contact with an engineer who had been at BNR and Nortel for  $7\frac{1}{2}$  years in the

microwave division, followed by the TDMA base station group and finally, the OC-192 fiber optic group before being laid off like everyone else. At the very end, he was a technical advisor. During the boom period ending around 2001, he estimates that there were between 50 and 100 RF/microwave designers doing hardcore design in Ottawa covering all aspects of RF circuit design. This design work would range from wireless CDMA, TDMA and GSM base station circuits all the way to fiber optics OC-3 up to OC-768 circuit packs and everything in between. In 1994, he was working on the LNA for a 512 QAM 6 GHz radio. At one point, he recalled hearing Nortel was Agilent's second biggest test equipment customer in the world. "Seeing all the equipment we had in the huge labs here, it didn't surprise me." What was surprising to everyone was just how far this Goliath would fall.



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## Bienvenue – Welcome to IMS 2012



am very excited about this much discussed and anticipated year of 2012, which promises to be a special year for all of us. We certainly have a multitude of world events this year, and not just in sports, or in movies, or in economics, or in politics. For us, as microwave engineers, the most important event plays out right here in Montréal this summer: our IMS 2012 and Microwave Week! What could be more exciting than this?

On behalf of the entire IMS 2012 Steering Committee and the City of Montréal, I feel privileged and honored to invite you and your family to take part in this historic and unparalleled event this June.

It has been a long and eventful journey that started in the early 1950s in New York City with the formation of the IEEE MTT-S. This

journey has seen the creation and subsequent growth of IMS, the MTT-S flagship event and the largest gathering in the entire microwave community. This year, IMS finally comes to Montréal, Canada, a truly international destination. Not only is this the second time that IMS will be held outside the U.S., it also coincides with the 60th anniversary of MTT-S, which makes this a truly unique event to be remembered in the future.

During Microwave Week, June 17 – 23, you will be able to register for and participate in various technical programs in connection with three events, namely the Radio Frequency Integrated Circuits (RFIC) Symposium (www.rfic2012.org), IMS (www.ims2012.org), and the 79th Automatic Radio Frequency Techniques Group (ARFTG) Conference (www.arftg.org).

In spite of the current uncertain economic situation and financial worldwide turmoil, we are expecting to have about 10,000 attendees and 600 exhibitors with over 900 booths joining us. This high expectation is encouraged by early indications that point to a very successful symposium. We have already broken historic IMS records including an all-time record number of technical paper submissions from 49 different countries and regions, an all-time record number of MicroApps presentation proposals, and never before have there been so many commercial exhibit booth reservations early on. We are building not just a larger IMS, but also a

**KE W**U IMS 2012 General Chairman

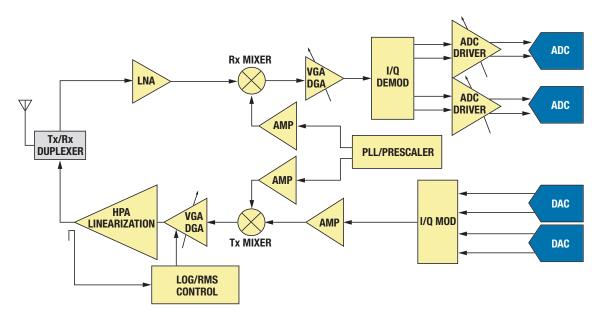


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everything to everyone with easy access to everywhere.

IMS 2012 will be held in the colorful Palais de Congrès de Montréal, which is located in the heart of this vibrant city and surrounded by the old world charm of this historic town and the modern cosmopolitan dynamics of the new city.

Everything is within a short walking distance. The area is accessible by subway, bus and car from other parts of the city.

Montréal downtown is a very animated place full of people of all ages. This is also one of the safest metropolitan areas in the world. Most of the 3.5 million local residents are multilingual with multiple cultural backgrounds. To facilitate and enrich your stay in Montréal, we have prepared a set of local tours and quest programs for all interested parties and family members during Microwave Week. You will also find that your presence at Microwave Week will add a special international flavour to Montréal's beautiful summer decorated by its well-known festivities.

IMS 2012 will present an outstanding technical program and plenary keynote addresses, in conjunction with workshops, short courses and special sessions including two special memorial sessions. Student Paper Competitions, Student Design Competitions and the Graduate Design Challenge are organized to highlight the outstanding contributions of the new generation of researchers from our academic communities. These activities have always attracted large crowds in the technical sessions, interactive forums and special presentations. Awardees will be announced during the Awards Banquet on Wednesday.

In conjunction with the excellent technical programs and abundant social activities, you have the opportunity to attend and explore the world's largest exhibition dedicated to the RF and microwave industry. This exhibition will also feature university and academic laboratory booths. We will see a strong presence of international companies. Therefore, we expect to have more business interactions and exchanges among our well established exhibitors, new exhibitors and attendees. In addition, the regular historical exhibit, showing how far our technical community has come, will be

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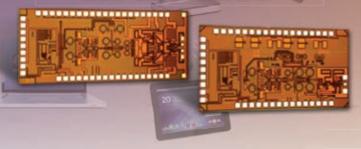
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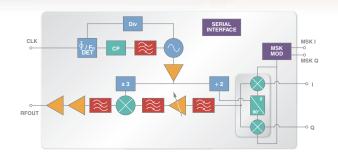


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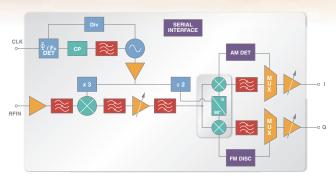


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57 - 64	60 GHz Integrated Transmitter	12 dBm	38	17	-86	0.8	HMC6000
57 - 64	60 GHz Integrated Receiver	6 dB	67	65 @ 1 dB Step	-86	0.61	HMC6001

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enhanced by a healthy addition of Canadian historical components. Another noteworthy highlight is the much-anticipated MicroApps presentations during the commercial exhibition.

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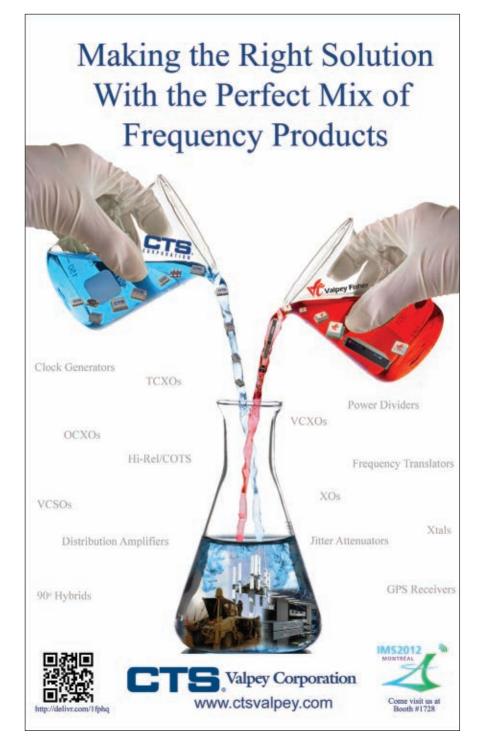
day exhibition. Exhibition hours are Tuesday, June 19th, 9:00 AM to 5:00 PM, Wednesday, June 20th, 9:00 AM to 6:00 PM, and Thursday, June 21st, 9:00 AM to 3:00 PM. On Wednesday, we will also have the traditional Industry-Hosted Cocktail Reception held on the exhibition floor starting at 5:00 PM. You

should not miss this opportunity to interact with exhibitors while enjoying complimentary refreshments and snacks.

This year's motto "Microwaves without Borders" or "Micro-ondes sans Frontières" not only reflects our unique French heritage and culture in North America but also the international cooperation and spirit of our community. The successful organization of such a Microwave Week requires a huge effort and the selfless dedication of many volunteers. I would like to thank those who have already and will continue to contribute including the Steering Committee, our TPRC, our exhibit manager MP Associates, our IEEE meeting planner, our sponsors, our media partners, and of course the MTT-S AdCom. I would like to particularly express my appreciation to Microwave Journal and its staff for the help they have provided.

Again, I warmly welcome you and your family to this historic and unparalleled event and hope that you will find time to explore the friendly atmosphere of Montréal with its myriad of attractions, wealth of activities, exquisite cuisines and excitement of life, while also enjoying our popular professional meetings and social gatherings. You can find useful information on the city of Montréal at www.tourism-montreal.org. In addition, there are many famous festivals and international happenings like the world famous Formula 1 Grand Prix and the Jazz Festival, for your enjoyment right before and after Microwave Week.

This is a very rare opportunity for all of us to celebrate this historic event in Montréal, which you cannot afford to miss. Please go to http://ims2012.mtt.org for more information and the latest news for your attendance at IMS 2012 and Microwave Week. I do hope that you have received or downloaded your copy of the Program Book for detailed information. A bientôt! See you soon! ■



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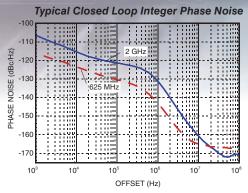
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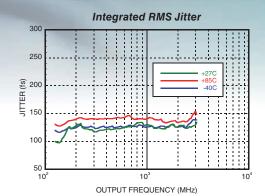


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NEW!	500	Integer Mode PLL (x1, x5, x10)	Defined by VCXO	Defined by VCXO	140	0.005	5	-208	HMC1031MS8E	
NEW!	3000	Clock Generator with Fractional-N PLL+VCO	118 / 78	-165	350	0.86	i	-227 / -230	HMC1034LP6GE	
-	Max. Clock Rate (GHz)	Function	Input	Output	Phase Jitter (12 k to 20 MHz)	Rise / Fall Time (ps)	Disable Mode	Power Supply (V)	Part Number	
	8	1:9 Fanout Buffer	LVPECL, LVDS, CML, CMOS	LVPECL	8 fs RMS	65	Yes	3.3	HMC987LP5E	
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## RFIC 2012 General Chair's Message



lEEE Radio Frequency Integrated Circuits (RFIC) Symposium, which will take place in Montréal, Canada (www.RFIC2012.org) on June 17-19, 2012. Our symposium, held in conjunction with the IEEE MTT-S International Microwave Symposium, opens Microwave Week 2012 with three days focused exclusively on RFIC technology and innovation.

This year's venue is the Palais des Congrès de Montréal. Montréal, a 3.6 million metropolis, is the second largest French-speaking city in the world - located on an island at the junction of the St. Lawrence and Ottawa rivers. Montréal is a very walkable, dense city with a well-preserved historic center besides a modern downtown, plenty of public spaces and parks, a quick and clean transit system, beautiful architecture and neighborhoods, and of course lots of sidewalk cafés for people watching. We hope that you take full advantage of these opportunities on your visit.

Some of the prevalent themes in this year's conference include the emergence of Terahertz technology and applications, and the continuing expansion of smartphones, multi-band and re-configurable RF, and silicon millimeterwave design. As usual, the latest advances in RFIC design from the device level to the system level

will be covered in various formats including a complete workshop program taught by RFIC experts, panel sessions featuring respected industrial and academic voices in the RFIC community, and an exciting two-day technical program.

The 2012 RFIC Symposium will kick-off on Sunday, June 17 with a full lineup of half-day and full-day workshops covering a wide array of topics. Workshop topics will include mm-Wave Silicon PAs, Fast-Settling RF Frequency Synthesis, RF at the Nanoscale, RF Spectrum Sensing and Signal Detection, ICs for Biomedical Applications, Digital Transmitters, Short-Range Near-Field Communications, RF Front-End and Transceiver Techniques, Multi-Standard Radio Coexistence, 3D Integrated Circuits, recent developments in active/ passive mixer design and highspeed wireline transceivers, and advances in noise analysis of RF circuits and front-end modules for mobile applications.

The Plenary Session will then be held on Sunday evening with keynote addresses given by two renowned industry leaders. They will share their views and insights on the direction and challenges that the RFIC design community is facing. The first speaker is Professor Thomas Lee of Stanford University, one of the pioneers of CMOS RF research for wireless communications. He will present a talk titled "Terahertz Electron-

ics: The Last Frontier." The second speaker is Robert Gilmore, VP of Engineering at Qualcomm. He will bring perspective and knowledge from one of the leading wireless suppliers in the industry. The title of his talk will be "Towards the 5G Smartphone: Greater System Capacity, More Bands, Faster Data Rates, Advanced Applications and Longer Battery Life."

Immediately following the Plenary Session, conference attendees can gather at the RFIC Reception, to be held outdoors this year, which provides a relaxing time for all to mingle with old friends and catch up on the latest news.

The technical program will then commence on Monday and Tuesday with 23 technical sessions featuring a total of 126 papers. The RFIC technical sub-committees were re-organized this year to align with the growing trends in industry and academia. Subcommittees were formed in the areas of low-power transceivers (RFID, NFC, ZigBee, Sensor Nodes, WPAN, WBAN, and biomedical) and reconfigurable front-ends (SDR/Cognitive radio, Wideband/ Multi-band Front-ends, Digital RF circuits/architectures). Technical sessions will feature papers on advances in LNA design and SDR front-end techniques, millimeter-

**ALBERT JERNG** RFIC 2012 General Chairman

## RFMD.

## **High-Performance Symmetric Switches for Communications Systems**



RFMD offers a wide selection of broadband high-performance symmetric switches suitable for applications in the cellular, 3G, LTE, and other high-performance communications systems. Covering single-pole double-throw (SPDT), double-pole double-throw (DPDT), and single-pole triple-throw (SP3T), these products are ideal for use in high-performance and space-constrained applications. Each switch is 3V and 5V positive logic compatible.

#### **SPECIFICATIONS**

Switch Type	Freq Range (MHz)	Insertion Loss (dB)	Isolation (dB)	Input P1dB (dBm)	Control Voltage (V)	Package (mm)	Part Number
SPDT	LF to 6000	0.75	65.0	35.5	5	4 x 4 QFN	RFSW6124
SP3T	LF to 6000	0.5	27.0	33.0	5	1.5 x 1.5 DFN	RFSW6131
DPDT	LF to 6000	0.65	33.0	35.5	5	3 x 3 QFN	RFSW6223

#### **FEATURES**

#### **RFSW6124**

- · LF to 6000MHz operation
- Symmetric SPDT
- Insertion Loss: 0.75dB (2GHz)
- Isolation: 65dB (2GHz)
- IIP3: 47dBm
- P1dB: 35.5 at 5V

#### **FEATURES**

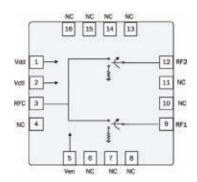
#### RFSW6131

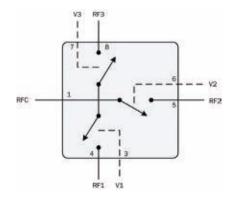
- LF to 6000MHz operation
- Symmetric SP3T
- Insertion loss: 0.5dB (2GHz)
- Isolation: 27dB (2GHz)
- IIP3: 56dBm
- P1dB: 33dBm at 5V

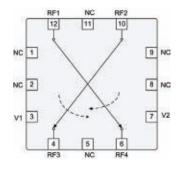
#### **FEATURES**

#### **RFSW6223**

- . LF to 6000MHz operation
- Symmetric DPDT
- Insertion loss: 0.65dB (2GHz)
- Isolation: 35dB (2GHz)
- IIP3: 56dBm
- P1dB: 35.5dBm at 5V















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The technical program features a strong set of industry papers from leading wireless RFIC companies such as Mediatek, Skyworks, NXP, ST Micro, Infineon, IBM, Broadcom, Anadigics, Marvell, Renesas and Analog Devices. There will also be an invited paper from Qualcomm titled "The Path Towards Gb/s Wireless LANs." On Tuesday afternoon, the technical program will conclude with the Interactive Forum which features 24 poster presentations. The poster session gives attendees the chance to speak directly with authors regarding their work in an informal setting.

The conference will also hold lunch-time panel sessions on Monday and Tuesday on several interesting topics relevant to the present and future of RFIC development. The Monday panel session is entitled "THz Integrated Circuits: Do Future Markets Support Highly Integrated Siliconbased IC Development?" and will explore the applications and markets that may drive the development of terahertz technology in silicon. The Tuesday panel session is entitled "RF Scaling: Can It Keep Up With Digital CMOS? Should It?" and will see panelists debate the pros and cons of scaling RF circuits in deep sub-micron CMOS technology. Be sure to attend these lively and entertaining events.

On behalf of the RFIC Steering Committee, I would like to extend a warm welcome to attend this year's 2012 RFIC Symposium. We are looking forward to an exciting program and seeing all of you this June in Montréal!

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## 79th ARFTG Microwave Measurement Conference



relcome to the 79th Automatic RF Techniques Group (ARFTG) Microwave Measurement Conference being held at the Palais des Congrès de Montréal, on Friday, June 22, 2012. The conference will include technical presentations, an interactive forum and an exhibition; all to give you ample opportunity to interact with your colleagues in the RF and microwave test and measurement community.

The conference theme is "Non-linear Measurement Systems" and we are looking forward to the invited talks of Dr. Jacques Sombrin on "Future Test Benches for the Optimization of Spectrum and Energy Efficiency in Telecom Non-linear RF Components and Amplifiers" and Dr. Thibault Reveyrand on "New Sampling Paradigm Dedicated to RF Ultra-Wideband Receivers." The contributed conference papers focus on nonlinear measurement systems, calibration issues, on-wafer measurements,

uncertainty, broadband and millimeter-wave measurements, and other areas of RF and microwave measurement.

Also, be sure to check out the joint ARFTG/IMS workshops on "Overview of Advanced Dielectric Measurement Techniques" and "Device model extraction based on Vectorial Large-Signal Measurements" on Monday, as well as the NVNA Users' Forum on Thursday afternoon. The NVNA Users' Forum is an informal discussion group devoted to sharing information and issues related to instrumentation utilized in vector large-signal analysis of microwave circuits and systems that contain nonlinear elements. This event is open to all ARFTG, IMS and RFIC attendees.

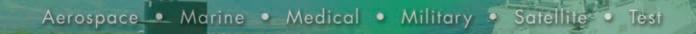
An important part of any ARFTG Conference is the opportunity to interact one-on-one with colleagues, experts and vendors in the RF and microwave test and measurement community. Whether your interests include high-

throughput production or one-ofa-kind metrology measurements, complex systems or simple circuit modeling, small to large signal measurements, phase noise or noise figure or DC to lightwave, you will find similarly interested technologists. Starting with breakfast, continuing through two exhibition/interactive forum sessions and the luncheon, there will be ample opportunity for discussion with others facing similar challenges. Attendees find that these interactions are often the best source of ideas and information for their current projects, so come and join us.

Full details of the technical program and conference are available at: www.arftg.org.

ARFTG Conference registration is available through the IMS website at: www.ims2012.org.

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# Canada

# IMS 2012 MicroApps



he Microwave Application Seminars (MicroApps) scheduled for the Palais des congrès de Montréal (Montréal Convention Center), June 19-21, 2012, as part of IMS 2012 – is a series of concise application note technical presentations given by exhibitors that are distinct and separate from yet complementary to the IEEE technical sessions. MicroApps are engineering topics of interest to the microwave community and cover new products, noteworthy state-of-the-art materials, components and measurement tools, and novel manufacturing and design techniques that incorporate the exhibitor's products and technologies in an application-centric setting.

This year's program is the most successful yet, offering more than 79 presentations on a diverse range of topics that include hardware, software and test. There will be 76 application notes, two keynote addresses and one panel session.

This year, Wednesday admission to the exhibit floor and also to the MicroApps Symposium is free. This means even more can take advantage of the special talks that

day, which include a keynote presentation, "James Clerk Maxwell Part II" by Dr. James Rautio and the Microwave Journal Panel Session, "Device Characterization Methods and Advanced RF/Microwave Design." This special panel session takes place in the MicroApps theatre from 12:00 to 1:30 PM on Wednesday. This session will have leading companies in the field

### **GaN PANEL SESSION**

### Where Are the Emerging RF Market Opportunities for GaN?

Join Strategy Analytics and Microwave Journal for a special panel of industry leaders to explore the business opportunities for GaN. Each industry expert will make a brief presentation followed by a question and answer session with the panel. Complimentary breakfast will be served.

Wednesday, June 20<sup>th</sup> 8:00-10:00 AM Palais des Congrès, Room 516 make presentations on the latest technology and techniques available followed by a question and answer period with the presenters. Attendees can also grab a whiskey shot Wednesday evening at the industry-hosted reception in honor of Maxwell and his Scotland heritage (sponsored by Sonnet).

MicroApps sessions are open to everyone, thanks to sponsorship by Agilent Technologies. The MicroApps theatre is conveniently located in the midst of the exhibits. The complete and up-to-date MicroApps Symposium schedule can be found in the IMS Program Book or online at http://ims2012.mtt.org. A Micro-Apps CD of all the presentations will be available for free to all, and those who are unable to attend in person will be able to order the CD from Agilent, watch the Microwave Journal webcast of the Panel Session and view the virtual presentations online at the IEEE.tv website.

Come to MicroApps, learn and enjoy. We look forward to seeing you in Montréal, Canada.

JAMES WEILER

IMS MicroApps 2012 Chair

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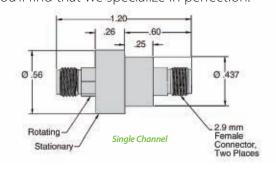
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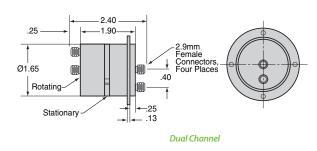
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### **SINGLE CHANNEL SPECIFICATIONS:**

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VSWR	DC - 10 GHz	1.20 : 1 MAX.
	10 - 26 GHz	1.35 : 1 MAX.
	26 - 40 GHz	1.75 : 1 MAX.
WOW	1.05 MAX.	
INSERTION LOSS	DC - 10 GHz	0.2 dB MAX.
	10 - 26 GHz	0.4 dB MAX.
	26 - 40 GHz	0.6 dB MAX.
PEAK POWER	Egual to conr	nector rating

### **DUAL CHANNEL SPECIFICATIONS**

DOAL CHAINEL	of Echileations.	
ELECTRICAL	Channel 1	Channel 2
FREQUENCY	7.0 - 22.0 GHz	29.0 - 31.0 GHz
VSWR	1.50:1 MAX.	1.70:1 MAX.
WOW	0.15	0.25
INSERTION LOSS	0.5 dB MAX.	1.0 dB MAX.
ISOLATION	Channel to Channel	50.0 dB MIN.



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# Canada 2

# **IMS 2012 Social** Media Scene









ast year, in preparation for MTT-S IMS, I wrote about Twitter (and related apps) starting to be used by RF/microwave companies. At that time, social media had not really caught on in our industry. What a difference a year makes as many companies and individuals are now using social media as one of their conduits for marketing efforts. Numerous companies and individuals now have hundreds or even thousands of Twitter followers and Facebook fans. While the use of social media in our industry is still not widespread, more and more companies are getting involved on a daily basis.

Twitter continues to be a powerful and popular social media tool. As you plan and execute your marketing programs for IMS 2012, don't forget to use the hashtag #IMS2012 in your Tweets. Spread the word about activities that you are planning, events you are attending, talks you are giving and keep everyone abreast of the best places to visit while in Montréal. Microwave Journal will be displaying a Twitter feed on our Online Show Daily microsite that is the official landing page of the Cyber Café at IMS 2012. Follow us and others involved in the show so you can keep up to date in real-time about what is going on at the conference and exhibition.

A couple of creative social media supporters are teaming up this year to run the Passport to IMS 2012 Montréal program. Every participant will receive a passport with 12 exhibitors listed on it and will visit the booths to get their passport stamped. After the passport is completed, participants can turn them in to the Microwave Journal booth #2018 to be entered into several prize drawings. The unique part of the program is that it integrates the use of social media by having participants post photos on Facebook and Tweet about products and giveaways at the booths (visit www. landingportal.com/IMSpassport for more details).

Turning to new trends on the social media scene, Pinterest has been growing rapidly in popularity even though it has been around for a few years. Pinterest is a virtual bulletin board site where people can put together boards of their favorite photos that link back to the web pages where they appear. Businesses are just starting to find uses for Pinterest, kind of in the state where Twitter was a few years ago. Consumers first jump in and as the user base grows, businesses start to find ways in which they can generate traffic to their content.

Microwave Journal is one of the first in this industry to use Pinterest and will be creating boards using products from our IMS 2012 Product Showcase (existing boards can be viewed at www.pinterest.com/ pathindle). For IMS 2012, we will

develop Pinterest boards by product category (Software/EDA, Test/ Measurements, Components, etc.) using pictures of products that will be featured at the exhibition. The pictures will link to descriptions of what the company is featuring at the show including the specific product "pinned" on the board. These will be available on our Online Show Daily microsite.

Over the past year, the biggest rise in popularity for a social media site that we have seen has been on LinkedIn. As an example, Microwave Journal started the RF and Microwave Community group a few years ago with some limited success over the first couple of years. Now the group has close to 12,000 members and is still growing. There are daily posts for various discussion topics, technical questions, promotional items and of course, an active job opportunity section. Microwave Journal strives to be at the forefront of social media marketing and will continue to innovate in this area as we do in print, online and at events as a full service media partner.

When creating or growing your social media presence, remember that social media is just one component of an integrated marketing plan that should utilize many channels in order to promote a brand or product.

#### PATRICK HINDLE

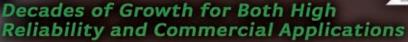
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Tuesday June 19th 11:05 am John Coonrod "Bonding Materials used in Multilayer Microwave PCB Applications"

Tuesday June 19th 3:05 pm Al Horn "Reducing Active Device Temperature Rise and RF Heating Effects with High Thermal Conductivity Low Loss Circuit Laminates"

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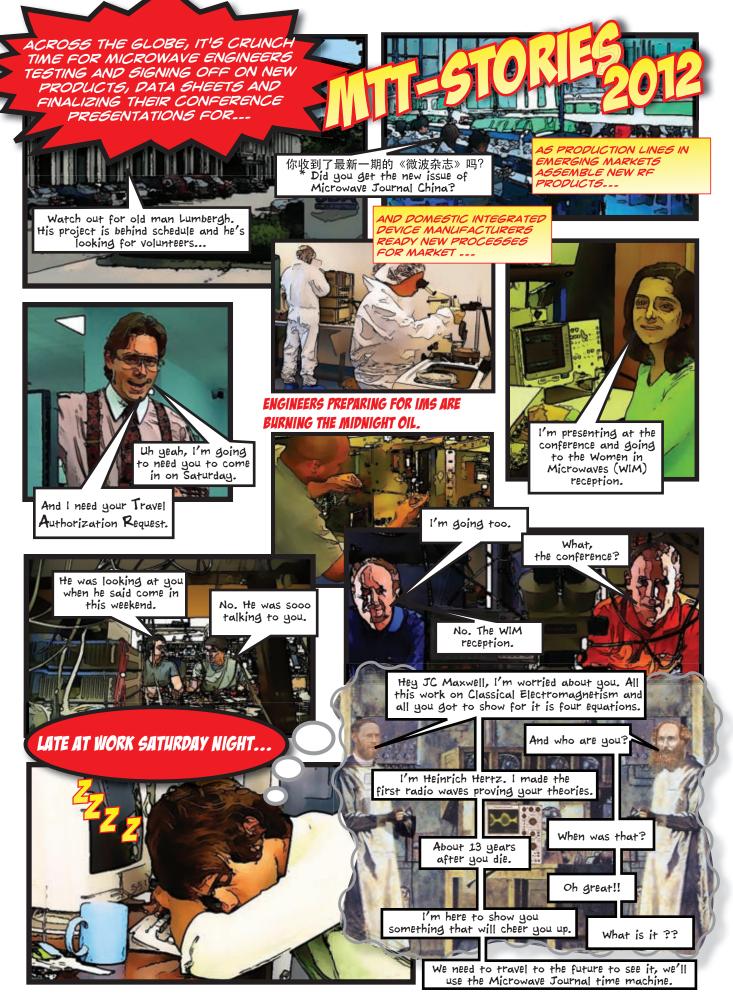


















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Model No. CA01-2110 CA12-2110 CA24-2111 CA48-2111 CA012-3111 CA1218-4111 CA1826-2110	Freq (GHz) 0.5-1.0 1.0-2.0 2.0-4.0 4.0-8.0 8.0-12.0 12.0-18.0 18.0-26.5	Gain (dB) MII 28 30 29 29 27 27 25 32	Noise Figure (db) 1.0 MAX, 0.7 TYP 1.0 MAX, 0.7 TYP 1.1 MAX, 0.95 TYP 1.3 MAX, 1.0 TYP 1.6 MAX, 1.4 TYP 1.9 MAX, 1.7 TYP 3.0 MAX, 2.5 TYP	Power-out @ PI +10 MIN +10 MIN +10 MIN +10 MIN +10 MIN +10 MIN +10 MIN	+20 dBm +20 dBm +20 dBm +20 dBm +20 dBm +20 dBm +20 dBm	VSWR 2.0:1 2.0:1 2.0:1 2.0:1 2.0:1 2.0:1 2.0:1
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CLA24-4001 CLA26-8001 CLA712-5001 CLA618-1201	2.0 - 4.0 2.0 - 6.0 7.0 - 12.4 6.0 - 18.0	-28 to +10 c -50 to +20 c -21 to +10 c -50 to +20 c	Bm +7 to +1 Bm +14 to +1 Bm +14 to +1	l dBm 8 dBm 9 dBm	+/- 1.5 MAX +/- 1.5 MAX +/- 1.5 MAX +/- 1.5 MAX	2.0:1 2.0:1 2.0:1 2.0:1
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CA001-2110 CA001-2211 CA001-2215 CA001-3113 CA002-3114 CA003-3116 CA004-3112	0.01-0.10 0.04-0.15 0.04-0.15 0.01-1.0 0.01-2.0 0.01-3.0 0.01-4.0	18 24 23 28 27 18 32	4.0 MAX, 2.2 TYP 3.5 MAX, 2.2 TYP 4.0 MAX, 2.2 TYP 4.0 MAX, 2.8 TYP 4.0 MAX, 2.8 TYP 4.0 MAX, 2.8 TYP 4.0 MAX, 2.8 TYP	+10 MIN +13 MIN +23 MIN +17 MIN +20 MIN +25 MIN +15 MIN	+20 dBm +23 dBm +33 dBm +27 dBm +30 dBm +35 dBm +25 dBm	2.0:1 2.0:1 2.0:1 2.0:1 2.0:1 2.0:1 2.0:1
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### Dan Massé, Associate Technical Editor

## Raytheon to Help U.S. Army Better Detect Rocket, Artillery and Mortar Threats

aytheon Co. has been awarded a \$45.5 million contract for the prototype build of the Ku-Band Multi-Function RF System (MFRFS) Sense and Warn (S&W) radars for the U.S. Army. The contract is a follow-on to an ongoing effort being performed by Raytheon to improve the performance of the Counter Rocket Artillery and Mortar (C-RAM) S&W systems currently fielded at forward operating bases in theater of operations.

Under the contract, Raytheon will procure long-lead material and subsystems for Ku-Band MFRFS prototype systems to be built in 2012. The work is in support of Program Directorate C-RAM under PEO Missiles and Space in Huntsville, Ala. The development of the Ku-Band MFRFS system heavily leverages technology developed by Raytheon on the Army's Future Combat Systems (FCS) program.

As a precursor to the Ku-Band MFRFS variant, Raytheon developed, tested and deployed a Low Quadrant Elevation (QE) MFRFS C-RAM S&W system in 14 months, utilizing residual assets from the FCS program. Eighteen additional Low QE systems, for C-RAM applications, will be deployed during the first half of 2012 using FCS assets. Both the Low QE MFRFS and the Ku-Band MFRFS sys-

"The MFRFS
C-RAM mission is
extremely important
in that it provides a
life-saving capability
to our men and
women in uniform."

tems provide improved S&W times, virtually eliminate false alarms and improve coverage of currently fielded C-RAM systems. The Ku-Band system will further improve performance and reduce logistics costs.

"The MFRFS C-RAM mission is extremely im-

portant in that it provides a life-saving capability to our men and women in uniform," said Glynn Raymer, vice president of Combat and Sensing Systems for Raytheon's Network Centric Systems business. "By reliably providing them with additional warning of incoming threats, we dramatically improve their survivability. And, by reusing existing technology, we are able to minimize the cost and risk of rapidly fielding improved C-RAM systems," Raymer added.

## U.S. Army Awards Contract for AN/TPQ-53 Firefinder Radar

he U.S. Army Product Manager for Radars (PdM Radars) awarded a contract recently to Lockheed Martin for the AN/TPQ-53 Firefinder Radar. The award is a Firm Fixed Price contract for \$881 million with the base year and two option years, which could yield up to 51



Source: U.S. Army

systems. The base year is \$166 million that will produce 12 systems. All training and testing support to include a Limited User Test as well as Initial Operational Test and Evaluation is covered by the contract.

The AN/TPQ-53 (formerly referred to as the EQ 36) provides improved operational and physical functionality over existing AN/TPQ 36 radars systems. The radar detects in-flight projectiles at greater rangers and determines and communicates the firing point locations with a high degree of accuracy. It does this with a low false alarm rate and with an improved coverage pattern. This capability allows for more effective detection and counter-battery actions.

"The AN/TPQ-53 will bolster the level of protection for Soldiers in the field, by expanding basic counterfire radar capabilities in both 90 and 360 degree modes," said Lt. Col. Robert Thomas, PdM Radars. "This is a great example of the Army and industry coming together to ultimately deliver a system that will greatly enhance situational awareness by providing the precise location of hostile indirect fire weapons."

### Harris Introduces Ultra-Light, High-Frequency Spaceborne Antenna Reflector

arris Corp., an international communications and information technology company, has introduced the first-ever fixed-mesh antenna reflector that supports emerging requirements for high-throughput, high-reliability Ka-Band and higher frequency satellites. The solution is ideal for satellite Internet, HDTV and cellular backhaul providers, and businesses that transfer large amounts of data between remote locations, such as oil and gas companies and maritime users. The fixed-mesh reflector design significantly lowers the antenna's mass for a given aperture size as compared to traditional solid reflectors. The lower mass is made possible by incorporating a flight-proven mesh surface instead of a traditional solid reflector membrane surface. Other benefits and features include:

- The new design is not sensitive to acoustic loading during launch, which reduces the overall structure and mass of the satellite.
- The reflector greatly increases the gain and potential



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### **Defense News**

spot beams available to satellite manufacturers and service providers. The increased frequency reuse provided by additional spot beams enables higher data rates required by providers of bandwidth-hungry services.

 The reflector features flight-proven design elements refined during development and production for U.S. government and commercial programs, including the application of reflective mesh; unique, high-accuracy surface-shaping technology; and thermally stable materials. The highly reflective mesh surface provides excellent RF reflectivity without exotic surface treatments required for high-frequency solid reflectors.

 The antenna reflector's projected aperture ranges from 2.6 to 3.5 meters in diameter, with a compact stowed configuration suitable for most launch vehicles. Its mass is half that of conventional solid reflector technology, which greatly increases potential mission performance compared to currently employed technologies.

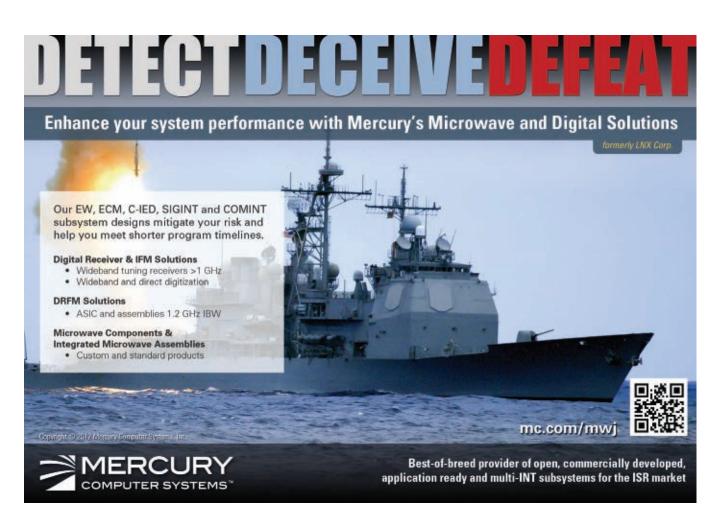
"This new fixed-mesh antenna reflector is a natural extension of our existing offerings and addresses the emerging need for larger apertures at a fraction of the mass and weight of conventional solid reflectors," said Sheldon Fox, group president, Harris Government Communications Systems. "Harris has a 35-year legacy of providing

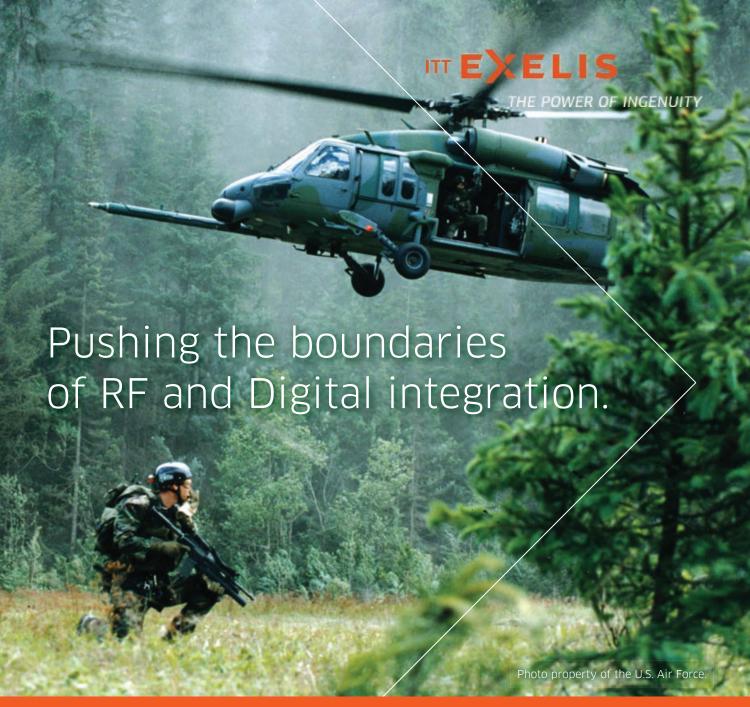
high-performance antenna solutions with unmatched performance, and this solution supports the ever-increasing global demand for higher bandwidth capacity."

With more than 50 antenna reflectors in orbit, Harris is the leading supplier of large reflector apertures and unfurlable mesh reflector antenna systems for all orbital regimes. The company's offerings span UHF band through Ka-Band, in sizes rang-

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ing from 2.6 meters to the world's largest commercially available 22-meter reflector. Harris reflector products have the highest surface accuracy design in the industry, while substantially exceeding the specified mean mission duration of the spacecraft and payload.







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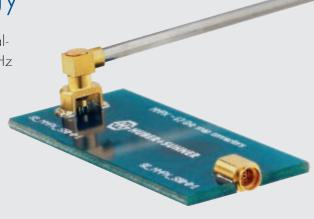




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### Indian Operators Prime Networks for Mobile Broadband Uptake

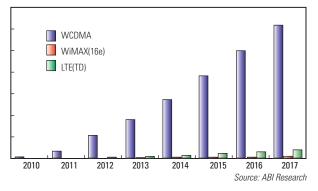
The Indian mobile subscriber market has demonstrated strong growth in the past decade or so, but when it comes to the adoption of mobile data services, the results are more mixed," commented Jake Saunders, vice president of forecasting at ABI Research, following the company's new study – Indian Mobile Broadband Market. He continued, "Yes, total wireless data subscribers stood at more than 370 million at the end of 2011, but only 17 million had access to WCDMA services; the rest are being served by GPRS/EDGE."

The report highlights the constraints behind the Indian mobile broadband sector and complications of the current regulatory scene, as well as market drivers for future growth. It indicates that the Indian market is full of potential. At the end of 2011, there were 900 million mobile subscribers. However, a note of caution is merited. The market is heavily fragmented, with more than 70 3G licensed circles. Considerable expectations were placed on 4G WiMAX, which failed to materialize. WCDMA and TD-LTE subscriber adoption will eclipse 90 million and 5 million respectively, by 2013.

There are a number of challenges to kick-starting the Indian mobile broadband market. The large landmass and population are two substantial reasons, but India's low average monthly revenue per user (\$3 to \$5) also constrains cash flow to fund infrastructure investments.

Addressing potential developments Philip Solis, ABI Research's research director, mobile devices, stated, "While 3G services are only now establishing a toehold in the Indian market, operators such as Aircel, Augure, and Infotel are turning to TD-LTE, a 4G technology of the time division variant, to help address the market potential for mobile data services. LTE offers the potential to change the cost equation of delivering mobile data services through increased spectral efficiency – not just in dense, urban communities but also rural towns and villages."

### Mobile Broadband Subscribers by Technology India, Forecast: 2010 – 2017



## **COST Receives Additional €10 Million from European Commission**

he European Commission Directorate-General for Research & Innovation has informed COST and the European Science Foundation (ESF) of its decision to allocate an additional €10 million to COST. This latest allocation raises the total budget for COST to €250 million, which was the maximum initially envisaged by the EU Seventh Framework Programme (FP7) subject to a mid-term evaluation.

COST is an intergovernmental framework for European Cooperation in Science and Technology, which implements networking activities for researchers, contributing to the European Research Area (ERA) goals and participating in the delivery of the Europe 2020 agenda.

"This further increase in the COST budget reveals the European Commission's trust in our intergovernmental

framework's ability to build excellence-driven networks by connecting high-quality scientific communities through a bottom-up inclusive approach throughout Europe

"...COST will continue to invest in science and technology activities..."

and worldwide. With these additional funds, COST will continue to invest in science and technology activities, thus reinforcing COST's contribution to Europe's research and innovation capacities by favouring trans-domain multidisciplinary networks and integrating the talent of the next generations," commented Dr. Ángeles Rodríguez-Peña, president of the COST Committee of Senior Officials (CSO).

"The ESF, as implementing agent for COST and the beneficiary of the COST II grant agreement with the European Commission, has indeed been asked to consider the additional annual financing of €13.4 million when submitting the annual Work Programme from now on. We are already preparing the respective annual Amendment 2012 for a total of €43.3 million in cooperation with the CSO and aim for a smooth approval process in June 2012," added Martin Hynes, chief executive of ESF.

### **HELIOS Makes Silicon Breakthrough**

esearchers in Europe have succeeded in presenting an integrated tuneable transmitter on silicon, for the very first time. The breakthrough is the result of the HELIOS (Photonics electronics functional integration on complementary metal oxide-semiconductor, CMOS) Project, which is backed under the Information and Communication Technologies (ICT) Theme of the EU's Seventh Framework Programme (FP7) to the tune of €8.5 million.

Experts from the Electronics and Information Technol-



### International Report

ogy Laboratory of the French Atomic Energy Commission (CEA-Leti) and III-V lab, a joint lab of Alcatel-Lucent Bell Labs France, in cooperation with Thales Research and Technology in the UK, believe the tuneable laser source integrated on silicon to be a groundbreaking achievement in efforts to secure fully integrated transceivers. Researchers at Ghent University and the Interuniversity Microelectronics Centre (IMEC) in Belgium, and the University of Surrey, UK, who designed the modulator, supported the research

The group from CEA-Leti and III-V lab also demonstrated single wavelength tuneable lasers, with a 21 mA

"Experts...believe the tuneable laser source integrated on silicon to be a groundbreaking achievement..." threshold at 20°C, a 45 nm tuning range and a side mode suppression ratio larger than 40 dB over the tuning range.

Commenting on the results, CEA-Leti France photonics program manager, Laurent Fulbert, said: "We are proud to

jointly present with III-V lab the results of the integrated silicon photonics transmitter and the tuneable laser. The ability to integrate a tuneable laser, a modulator and passive waveguides on silicon paves the way of further developments on integrated transceivers that can address several application needs in metropolitan and access networks, servers, data centres, high-performance computers as well as optical interconnects at rack-level and board-level.

### **EC Launches New Cluster Initiatives**

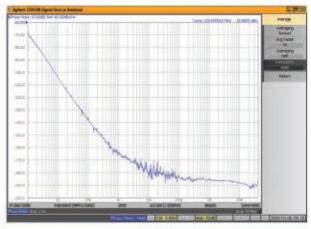
The European Commission has announced new and updated initiatives to assist small and medium-sized enterprises (SME) to go international. New projects will be launched to support clusters of SMEs so that they can benefit from the growth in Asia, Latin America, North America and Russia.

A new pilot action aims to upgrade the profile of 25 experts working in clusters to act as 'multipliers' and train other cluster managers to support SMEs in trading globally. Some 30 cluster benchmarking evaluators will be trained and 80 cluster organisations are expected to be benchmarked against clusters that are performing elsewhere so they can all learn from each other and perform more effectively. These cluster organisations will also sign up to the European Cluster Collaboration Platform, which will help them gain greater international exposure and ultimately new business and export opportunities for their SMEs.

The projects involve 20 organisations in Greece, Ireland, Hungary and Turkey encompassing further partners from Bulgaria, the Czech Republic, Croatia, Iceland, Poland, Portugal, Romania, Serbia, Slovakia and Spain. The overall EC contribution amounts to over €1.5 million.

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Calling these amplifiers "wideband" doesn't begin to describe them. Consider that both the ZVA-183X and ZVA-213X amplifiers are unconditionally stable and deliver typical +24 dBm output power at 1dB compression, 26 dB gain with +/- 1 dB flatness, noise figure of 3 dB and IP3 +33 dBm. What's more, they are so rugged they can even withstand full reflective output power when the output load is open or short. In addition to broadband military and commercial applications, these super wideband amplifiers are ideal as workhorses for a wide number of narrow band applications in your lab or in a production environment.

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		(GHz)	(dB)	(dBm)	(dB)	(1-9)
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All Sales	ZVA-183X+	0.7-18	26	+24	3.0	845.00
000	ZVA-213X+	0.8-21	26	+24	3.0	945.00
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### Commercial Market

Dan Massé, Associate Technical Editor



**LTE Small Cell Shipments Will Surpass** LTE Macro Base Station Shipments in 2014

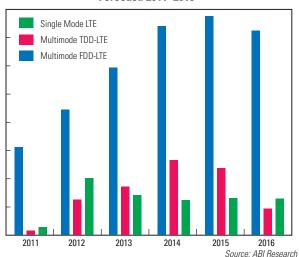
🦰 hanging cellular network paradigms are driving a shift in the architecture of base stations from traditional macrocells to distributed base stations and toward the growing use of small cell base stations. The primary drivers for this transition are the increasing data traffic demand and the OPEX and CAPEX cost savings inherent in deploying small cell equipment.

Operators will initially deploy small cell equipment as in fills on the pico and microcell layers, but will quickly transition to deploying them as a fundamental part of a network rollout. In fact, the number of LTE small cells sold (127,000) will surpass the number of LTE macrocells, forecast at 113,000, as early as 2014. However, LTE base station revenues will continue to be dominated by macro base station revenue with small cell revenue of \$1.09 billion representing only 5.2 percent of the total revenue of \$20.86 billion in 2014 and growing to \$4.44 billion or 23.9 percent of the total \$18.60 billion LTE base station market by 2016.

Equipment manufacturers have been quick to respond to this shift in RAN architecture. Ericsson acquired BelAir networks as part of its "HetNet" initiative, Nokia Siemens Networks announced Flexi Zone, Alcatel-Lucent continues to expand its lightRadio<sup>TM</sup> portfolio and Huawei has announced its AtomCell products.

Nick Marshall, principal analyst, networks, comments, "This mobile broadband-driven data storm is stretching traditional macrocell network capacity to the limit and driving the move to heterogeneous networks." Likewise, semiconductor suppliers are also positioning themselves to participate in this market with TI, Freescale, Cavium,

### LTE Macro Base Stations by Technology World Market, Forecast: 2011-2016



Mindspeed, and DesignArt among the manufacturers offering new "base station-on-a-chip" SoCs. "These base station baseband SoCs are among the most complex ICs on the market today and raise the bar in terms of complexity," says Marshall. ABI Research's new report, "The LTE Base Station Market," examines the ecosystem and outlook for LTE base stations. The report looks at base station topology and the uptake of small cells and remote radio heads (RRH) as elements of the distributed base station. The report also examines the merchant semiconductor baseband processor suppliers for these base stations.

### Maritime Satellite Communications Market Tops 5.5 Percent in Terminal Growth, \$1.4 B in Revenues

uroconsult, the leading international consulting and analysis firm specializing in the satellite and space sectors, recently forecast that the number of satellite communications terminals in the global maritime market will nearly double over the next decade, with a compound annual growth rate (CAGR) of 7 percent over the 10-year period. While MSS terminals are still expected to account for the majority of terminals deployed over the decade, VSAT service providers should gain significant market share

in terms of revenue in the coming 10 years.

In the second edition of the report "Maritime Telecom Solutions by Satellite, Global Market Analysis & Forecasts," provides Euroconsult an in-depth view of the dynamics determining growth in the maritime satcom sector, along with analysis and forecasts for

"Onboard bandwidth requirements keep growing, driving the maritime market in a direction quite beneficial to satellite communications."

the different levels of the value chain. The report offers a detailed review of the merchant shipping, fishing, passenger ship, leisure vessel, offshore and government segments. The breakdown between MSS applications and VSAT frequency bands is explored through each of these sections.

"Onboard bandwidth requirements keep growing, driving the maritime market in a direction quite beneficial to satellite communications," said Wei Li, senior consultant at Euroconsult. "Fully integrated IP applications providing Internet access, audio and video streaming, and the integration of ships into corporate networks generate significant capacity demand at sea."

Euroconsult said the number of terminals used for global maritime satellite communications grew at around 6 percent in 2011, while revenues at the satellite operator level increased by over 7 percent. The total size of the market reached about 317,000 active terminals in 2011 that gen-

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### **Commercial Market**

erated more than \$1.4 billion in revenues at the service provider level. Established MSS services and especially the emerging VSAT business contributed to the overall growth of the maritime satellite communications market.

The report also suggests that the proliferation of new Ka-Band based services, which allow much faster upload and download speed than either traditional VSAT or MSS, could expand the maritime market further. Inmarsat, the largest MSS operator, continues to ready its constellation of three Ka-Band satellites planned to be operational by 2014/2015. Euroconsult projects that by 2021, the VSAT market will account for the majority of satellite-based maritime communications revenues. Overall, Euroconsult predicts that the maritime satcom market will grow at a healthy rate over the next decade, but not as rapidly as in recent years. The expected slowdown of revenue growth is mainly due to decreasing airtime unit and equipment prices with the overall improvement of technology.

### Smartphone Shipments Will Eclipse All Other Handset Shipments Combined

lobal handset shipments will increase 29 percent from 1.7 billion in 2012 to 2.2 billion in 2016. The key driver of this growth will come from the smartphone

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segment, which is forecast to become larger than the ultra-low cost, low-cost, and feature phone segments combined by 2016. The total shipments of non-smartphones will grow 1.08 billion in 2012 to 1.09 billion in 2016 while smartphone shipments will grow from 643 million to 1.1 billion over the same period.

OEMs that have had historic success addressing the low-cost handset segments will be under tremendous pressure to shift their portfolio to smartphones. Considering that they currently serve consumers with low disposable incomes, these OEMs will need to deliver smartphones that are price competitive to low-cost handsets. "This emerging scenario could become a very dangerous situation for Nokia's handset business as the smartphone and feature phone segments will not be able to support each other in trying times," says Kevin Burden, vice president and practice director, mobile devices.

Low-cost OEMs that are shifting to smartphones, such as Huawei and ZTE, will be a key driving factor for the growth and innovation in the sub-\$150 smartphone segment. Low-cost smartphones are forecast to grow from 45 million shipments in 2012 to 170 million in 2016. "The writing is on the wall: either you have a successful smartphone strategy or you will have to steal market share to grow," says Michael Morgan, senior analyst, mobile devices.



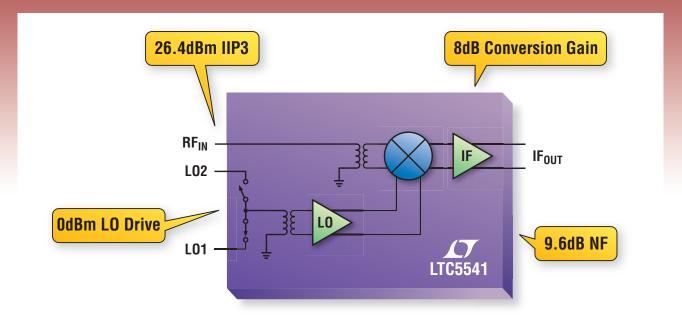
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Conversion Gain	8dB	8dB	8dB	8dB
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NF @ 5dBm Blocking	16.2dB	16.0dB	17.3dB	17.5dB
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### **INDUSTRY NEWS**

Analog Devices Inc. (ADI) has acquired Multigig Inc., a small, privately-held San Jose, Calif. company specializing in highly innovative high-performance clocking technology. The acquisition will enhance ADI's clocking capabilities in stand-alone and embedded applications, and will strengthen ADI's position in delivering high-speed data converters and signal processing solutions for their customers. Analog Devices acquired Multigig Inc. in a cash transaction completed on March 30, 2012. The engineers will become part of ADI's existing clock design team and will move to ADI's San Jose, CA facility.

**M/A-COM Technology Solutions Holdings** sold 6 million shares at \$19 apiece in its initial public offering. The company, which raised \$114 million from the offering, had expected to sell 5.6 million shares at \$17 to \$19 a share. At the IPO price, the company is valued at around \$860 million. The chipmaker, which plans to use part of the IPO proceeds to pay holders of its Class B convertible preferred stock, posted a net income of \$22 million in the three months ended December 30, 2011 on revenue of \$73 million. The company is backed by its chairman John Ocampo, who will hold about 57 percent stake in it after the offering.

**TriQuint Semiconductor Inc.** officially opened **TriQuint International Pte Ltd.**, its new international headquarters in Singapore. The facility will be the focal point for most international customers, suppliers and manufacturing partners and is located at the Changi Business Park, close to Singapore's Changi International Airport. This new office will offer dedicated resources in a wide variety of areas ranging from customer service to supply chain management.

**Anritsu Co.** announced that its VectorStar Broadband ME7838A vector network analyzer (VNA) system was used by **Modelithics Inc.** to validate the performance of its nonlinear diode models for W-Band Single Anode and W-Band ZBD flip chip Schottky diodes from **Virginia Diodes Inc.** Two-port series S-parameter measurements were made using the ME7838A and on-board probing with calibration reference at the component pad-stacks to validate the model's performance from DC to 125 GHz.

**AWR Corp.** has been issued a U.S. Patent by the United States Patent and Trademark Office for a "block-specific harmonic balance analysis system." Originally filed on December 3, 2008, U.S. Patent No. 8,131,521 addresses circuit simulation using multi-rate harmonic balancing. Specifically, the invention − known as MRHB<sup>™</sup> and first available within AWR's 2009 product release − speeds the design of complex circuits by enabling the effective reduction of analysis dimensions (e.g., frequency or time). AWR was also recently awarded U.S. Patent No. 7,346,480, entitled "Impedance Mismatch Modeling in a Data Flow or Discrete Time Based System Simulation."

**Digilent Inc.** and **Analog Devices Inc.** (ADI) unveiled two all-in-one analog design kits. The kits include access to downloadable teaching materials, online support, textbook, reference designs and lab projects to design and implement analog circuits as a supplement to their core engineering curriculum. The Digilent Analog Discovery Design Kit (\$99 USD) and the more advanced Digilent Analog Explorer Design Kit (\$199 USD) allow students to build and test a wide range of analog and digital circuits using their own PC without the need for any other equipment.

**Delta Electronics Manufacturing** announced its certification to AS9100:2009 (Rev C) Quality Management System (QMS) for Aviation, Space and Defense organizations. The AS9100 quality standard is based on ISO 9001 guidelines, as well as additional stringent requirements specific to the Aviation, Space and Defense industries. Among other changes, revision C brings the standard in line with ISO9001:2008 and expands the scope of coverage to include land and sea based systems for Defense applications.

NuWaves Engineering has been selected to join the University of Dayton Research Institute's Center for Unmanned Aerial System Exploitation (CUE) consortium. CUE was established in 2009 under a grant from the Ohio Third Frontier program to meet increasing demand for sensor and payload integration, systems analysis, and flight demonstration and test of unmanned aerial systems. Nu-Waves is pledging a minimum of \$50,000 of Independent R&D funds to advance the UAS electronic technologies.

### **CONTRACTS**

Rohde & Schwarz teamed up with 7Layers, an international group of engineering and test centers, to complete RF and protocol conformance testing on an LTE device developed for the United States 700 MHz (3GPP Frequency Band 14) Public Safety Broadband Network. Since public safety communications equipment requirements differ from the requirements of a commercial network device, public safety equipment needs to be thoroughly tested for LTE RF and protocol conformance as well as for specific user applications. By using the Rohde & Schwarz R&S TS8980 LTE RF conformance test system, 7Layers is working on device validation and certification of an LTE device for public safety, functional in 3GPP Frequency Band 14.

**Texas Instruments Inc.** (TI) and **6WIND** announced support within the 6WINDGate<sup>™</sup> software solution for TI's new scalable 28-nm multicore processors based on its recently announced KeyStone II multicore architecture. The 6WINDGate software provides a proven solution to the challenges of performance, scalability, software compatibility and time-to-market faced by developers of high-end



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2-WAY				201			77-2	
DSK-729S	800 - 2200	0.5 / 0.8	0.05 / 0.4	1/2	25 / 20	1.3:1	10	215
DSK-H3N	800 - 2400	0.5 / 0.8	0.25 / 0.5	1/4	23 / 18	1.5:1	30	220
P2D100800	1000 - 8000	0.6 / 1.1	0.05 / 0.2	1/2	28 / 22	1.2:1	5	329
DSK100800	1000 - 8000	0.6 / 1.1	0.05 / 0.2	1/2	28 / 22	1.2:1	20	330
DHK-H1N	1700 - 2200	0.3 / 0.4	0.1/0.3	1/3	20 / 18	1.3:1	100	220
P2D180900L	1800 - 9000	0.4 / 0.8	0.05 / 0.2	1/2	27 / 23	1.2:1	5	331
DSK180900	1800 - 9000	0.4 / 0.8	0.05 / 0.2	1/2	27 / 23	1.2:1	20	330
3-WAY						10.000		
S3D1723	1700 - 2300	0.2 / 0.35	0.3 / 0.6	2/3	22 / 16	1.3:1	5	316
A STATE OF THE PARTY OF THE PAR	Company of the Compan				10			

In excess of theoretical split loss of 3.0 dB
 With matched operating conditions

### HYBRIDS

Model #	Frequency (MHz)	Insertion Loss (dB) [Typ://Max.] 0	Amplitude Unbalance (dB) [Typ./Max.]	Phase Unbalance (Deg.) [Typ./Max.]	(dB) [Typ:/Min.]	VSWR (Typ)	Input Power (Watts) [Max.]	Package
90°					1.		- 1,13	
DQS-30-90	30 - 90	0.3/0.6	0.8/1.2	1/3	23 / 18	1.35:1	25	102SLF
DQS-3-11-10	30 - 110	0.5 / 0.8	0.6 / 0.9	1/3	30 / 20	1.30:1	10	102SLF
DQS-30-450	30 - 450	1.2 / 1.7	1/1.5	4/6	23 / 18	1.40:1	5	102SLF
DQS-118-174	118 - 174	0.3/0.6	0.4 / 1	1/3	23 / 18	1.35:1	25	102SLF
DQK80300	800 - 3000	0.2 / 0.4	0.5 / 0.8	2/5	20 / 18	1.30:1	40	113LF
MSQ80300	800 - 3000	0.2/0.4	0.5 / 0.8	2/5	20 / 18	1.30:1	40	325
DQK100800	1000 - 8000	0.8 / 1.6	1/1.6	1/4	22 / 20	1,20:1	40	326
MSQ100800	1000 - 8000	0.8 / 1.6	1 / 1.6	1/4	22 / 20	1.20:1	40	346
MSQ-8012	800 - 1200	0.2/0.3	0.2/0.4	2/3	22 / 18	1.20:1	50	226
180° ( 4-POR	rs)	CIV.		39		1	10	
DJS-345	30 - 450	0.75 / 1.2	0.3/0.8	2.5/4	23 / 18	1.25:1	5	301LF-1
N. Committee of the Com		0.0.40				-		

In excess of theoretical coupling loss of 3.0 dB

### COMPLERS

Model N	Frequency (MHz)	Coupling (dB) [Nom]	Coupling Flatness (dB)	Mainline Loss (dB) [Typ /Max.]	Directivity (dB) [Typ.Min.]	Input Power (Watts) [Max.] =	Package
KDS-30-30	30 - 512	27.5 ±0.8	±0.75	0.2 / 0.28	23 / 15	50	255 *
KBS-10-225	225 - 400	10.5 ±1.0	±0.5	0.6/0.7	25 / 18	50	255 *
KDS-20-225	225 - 400	20 ±1.0	±0.5	0.2/0.4	25 / 18	50	255 *
KBK-10-225N	225 - 400	10.5 ±1.0	±0.5	0.6/0.7	25 / 18	50	110N *
KDK-20-225N	225 - 400	20 ±1.0	±0.5	0.2/0.4	25 / 18	50	110N *
KEK-704H	850 - 960	30 ±0.75	±0.25	0.08 / 0.2	38 / 30	500	207
SCS100800-10	1000 - 8000	10.5 ±1.5	±2.0	1.2 / 1.8	8/5	25	361
KBK100800-10	1000 - 8000	10.5 ±1.5	±2.0	1.2 / 1.8	8/5	25	322
SCS100800-16	1000 - 7800	16.8 ±1.5	±2.8	0.7/1	14/5	25	321
KDK100800-16	1000 - 7800	16.8 ±1.5	±2.8	0.7/1	14/5	25	322
SCS100800-20	1000 - 7800	20.5 ±2.0	±2.0	0.45 / 0.75	12/5	25	321
KDK100800-20	1000 - 7800	20.5 ±2.0	±2.0	0.45 / 0.75	14/5	25	322

<sup>\*</sup> Add suffix - LF to the part number for RoHS compliant version.

Unless noted, products are RoHS compliant.



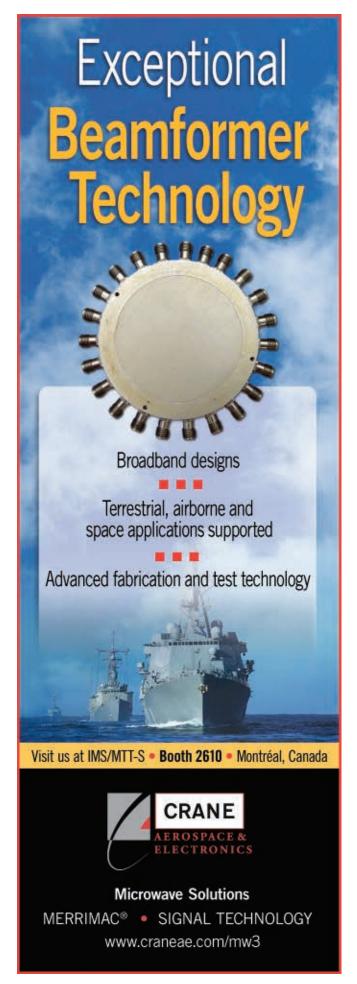
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<sup>.</sup> With matched operating conditions



### Around the Circuit

networking equipment. 6WINDGate includes a full set of control plane modules, a high performance networking stack and a wide range of data plane protocols that have been specifically optimized to deliver maximum performance on TI's KeyStone II-based multicore processors.

RF Micro Devices Inc. announced LG has selected RFMD to supply multiple components in support of the LG Optimus 4× HD and the Optimus 3D Max smartphones. RFMD components enabling LG's flagship smartphones include RFMD's PowerSmart® power platform, and RFMD's RF5501 802.11b/g/n Wi-Fi front end module. RFMD's PowerSmart features an RF Configurable Power Core<sup>TM</sup> that delivers multiband, multi-mode coverage of all cellular communications modulation schemes, including 4G, up to LTE 64QAM.

### **NEW MARKET ENTRY**

**Constant Wave Inc.** has launched a suite of consulting services to support the needs of RF design and test engineers. Their consulting services include: design or test process development and optimization; measurement, analysis and application assistance; and live product training. The services are customized to specific customer needs – whether engineers need help developing or improving a test process, or solving a measurement challenge.

### **PERSONNEL**

**Crane Co.** has announced the appointment of **Robert Tavares** as president of the Electronics Group of Crane Aerospace & Electronics, and **David Bender** as president of the Aerospace Group of Crane Aerospace & Electronics. As president of the Electronics Group, Tavares' responsibilities will include operations of Electronics Group locations and product solutions, including power, microwave and microelectronics. As president of the Aerospace Group, Bender is responsible for Aerospace Group site operations and product solutions, which include Fluid Management, landing systems, cabin systems and sensing & utility systems.

Laser Services Inc. has announced the hiring of several new team members in response to over a 15 percent growth in 2011. In the sales department, Phil Kendall has joined Laser Services as a sales representative bringing 20 years of sales, product, and operations management experience in the medical device and technical ceramics markets. Jamese Rivera, sales representative, comes to Laser Services with over 10 years of customer service experience in various manufacturing environments. Susan **Sullivan** has joined their administrative staff in the role of human resources representative and purchasing coordinator. Rounding out the new hires is **Decio Ferreria** in the Marketing Department, Jose Colon in Administration and Reception, and **Jonah Morton** in the Processing Department. Two Co-op students from Greater Lowell Technical High School, Iziah Martinez and Michael Chhun, are also onboard as active members of the Laser Services team.





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- · Smaller Volumes
- · Higher Isolation
- · Higher Power Levels
- . Faster Switching Speeds
- · Lower Insertion Loss

Model Number	Frequency Range	CW Power Rates	Peak Power Handling	Insertion Loss	Isolation	VSWR	Switching Speed	Size
SSHPS 0.96-1.22-3000	960-1220 MHz	250 Watts	3000 Watts	0.8 dB	60 dB	2,0;1	4 µsec	4.5 x 3.5 x 1.0 inches
SSHPS 1.2-1.4-4000	1200-1400 MHz	200 Watts	4000 Watts	0.7 dB	60 dB	1.6:1	4 µsec	4.5 x 3.5 x 1.0 inches
SSHPS 2.7-2.9-1000	2.7-2.9 GHz	100 Watts	1000 Watts	0.8 dB	40 dB	1.7:1	4 µsec	3.5 x 3.5 x 1.0 inches
SSHPS 2.9-3.1-1000	2.9-3.1 GHz	100 Watts	1000 Watts	0.8 dB	40 dB	1.8:1	4 µsec	3.5 x 3.5 x 1.0 inches
SSHPS 2.7-3.5-1000	2.7-3.5 Ghz	50 Watts	1000 Watts	0.9 dB	40 dB	2.0:1	4 µsec	3.5 x 3.5 x 1.0 inches
SSHPS 0.020-1.000-200	20-1000 MHz	200 Watts	1500 Watts	0.7 dB	25 dB	2.0:1	5 µsec	3.0 x 3.0 x 1.0 inches
SSHPS 0.225-0.450-400	225-450 MHz	400 Watts	2000 Watts	0.7 dB	40 dB	2.0:1	5 µsec	3.0 x 3.0 x 1.0 inches
SSHPS 1.0-2.5-200	1000-2500 MHz	200 Watts	1000 Watts	0.9 dB	25 dB	1.5:1	4 µsec	4.0 x 6.0 x 1.3 inches

### SSHPS 1.03-1.09-5000 Typical Data

- . Operation from 1030-1090 MHz
- Peak Power Handling of 5000 Watts
- . Insertion Loss = 0.4 dB nominal
- . Isolation = 58 dB typical
- . Operation into an Infinite VSWR
- . -40C to +70C Operation
- · Internal BIT
- < 5µSec Switching Speed
- Return Loss, All Ports = -14 dB nominal
- . 4.5" wide x 3.5" long x 1.0" high
- All switches High Power Tested & ESS Screened



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- 48 measurements for electrical signal characterization
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- Mast testing with 44 standard masks built-in
- · Pattern mask sync trigger
- FFT analysis

PicoScope model	9201A	9211A	9221A	9231A
12 GHz Sampling Oscilloscope	•		•	•
8 GHz optical-electrical converter		8	•	
USB port	•	•	•	•
LAN port		•		
Mask testing	•	•	•	•
Histogram analysis	•			
Clock recovery trigger		•	•	•
Pattern sync trigger		•	100	•
Dual signal generator outputs				•
Electrical TDR/TDT analysis				

### www.picotech.com/RF914





### Around the Circuit

### **REP APPOINTMENTS**

**Sea-Port Technical Sales** of Bellevue, Wash., is the company's new authorized distributors covering the Pacific Northwest for their entire range of USB Power Sensors. **Partner Electronic** of İzmir, Turkey is the new authorized distributors in Turkey for the company's entire range of fast, compact USB RF/μWave Power Sensors. Partner Electronic offers a wide range of products and services based on its extensive knowledge of RF, EMC, and test and measurement solutions and will be responsible for marketing and promoting Ladybug products in Turkey.

**RFMW Ltd.** and **MAST Technologies** announced a worldwide distribution agreement. MAST Technologies is a leading designer and manufacturer of RF absorbing materials. RFMW Ltd. is a specialized distributor providing customers and suppliers with focused distribution of RF and microwave components as well as specialized component-engineering support. According to the agreement, RFMW will distribute MAST Technologies broad portfolio of RF absorber material including cavity resonance and EMI absorbing elastomers, lossy and reticulated foam absorbers, as well as conductive and absorptive caulks and coatings that reduce EMI/EMC and RFI emissions.

Building on its successful model of local distribution centers in the U.S., UK, and Taiwan, **Mini-Circuits** announced that it is expanding its global network with **TejasRF.com**. Now customers all over India can enjoy the advantages of nominal factory prices in local currency, as well as local service and support, local freight, quicker response and faster delivery times than ever before possible, even for small quantity orders. TejasRF.com builds on the company's long-established presence and local sales support in India by offering online access to the entire Mini-Circuits catalog of over 6800 RF/IF and microwave products. With just a few clicks, Mini-Circuits' customers in India will get what they need, when they need it, as quickly and efficiently as possible.

**Richardson RFPD Inc.** has completed a global distribution agreement with **TRU Corp.**, a leader in the design, development and manufacture of custom, high performance RF/microwave interconnect solutions. TRU's high power cable assemblies provide power handling capabilities up to six times better than traditional RF assemblies. In addition to their distinctive high power cable assembly capabilities, TRU offers a wide range of standard and unique RF connectors. Richardson RFPD's worldwide field sales engineering teams are now assisting design engineers in integrating TRU connectors and cable assemblies into high power designs.

Vaunix Technology Corp. has announced the hiring of a new sales representative, Premier Measurement Solutions, to handle customer relationships in India. Premier Measurement Solutions Private Ltd. was formed by an expert team that has been in the test and measurement industry for close to two decades. They offer expertise in test automation for the wireless market, wafer level characterization, and CW signal generators and digital attenuators.



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# **Keep Assembly Closer to Home**



JIM MORGAN SemiGen Inc., Manchester, NH

utsourcing of manufacturing occurs across a broad spectrum of industries, and the philosophy of employing it is changing rapidly as companies are increasingly positioning themselves as brands as opposed to manufacturers. The outsourcing decision for RF/microwave (RF/MW) companies, however, has a unique set of circumstances as compared to conventional digital electronics. The straight-forwardness of digital electronics is conducive to high levels of automation and the employment of relatively unskilled workers. Quality and compliance in the digital world can also be determined through the use of functional test equipment working on the basis of logic one and zero levels whose repeatability, accuracy and calibration are relatively clear-cut. Moving these types of manufacturing and test procedures overseas thus becomes a relatively simple decision.

RF/MW manufacturing and test, on the other hand, often relies upon much more precisely defined, and sometimes difficult to define, procedures. In fact, RF/MW manufacturing is to a large degree an artisan-based process that is learned by being immersed in the business and is often passed along through ties of family or friendship. RF/MW testing also requires more complex tools such as spectrum analyzers and frequency counters whose

accuracy, repeatability and calibration have large variables. As a result, test specifications and methods are more critical and once again, rely more heavily on the knowledge and experience of operators and engineers.

These challenges have become even greater in the last decade or so. Product lifecycles have been compressed, increasing the pressure to get new products to market fast and putting pressure on manufacturing costs. Future sales of new products have become harder to predict so OEMs are understandably wary of investing in new manufacturing equipment. Meanwhile, performance expectations and multi-function requirements are increasing and the quest for reduction in footprints is omnipresent. Each of these issues leads to tighter manufacturing specifications and the risk of variables in the manufacturing process causing problems.

### **VALUE OF OUTSOURCING RF/MW MANUFACTURING**

A considerable number of RF/MW OEMs are addressing these challenges by taking a close look at outsourcing some or all of their manufacturing. One key advantage of outsourcing is that the OEM can focus on its core competency – which typically involves research and development, engineering, and sales and marketing – while

the contract manufacturer in turn focuses on its core competency. In many cases, greater concentration on engineering and marketing makes it possible for OEMs to improve their position in the marketplace.

Additionally, outsourcing to the right contract manufacturer often makes it possible to improve manufacturing and quality control. Contract manufacturers utilize leadingedge automated equipment and highly experienced staff members for multiple OEMs' products. This means the contract manufacturer can afford to maintain a higher level of manufacturing technology and expertise than a typical RF/MW OEM with less than \$100 million in sales. The right contract manufacturer will already have all or most of the equipment required to bring the product to market so the OEM's required capital investment will be eliminated or greatly reduced.

Outsourcing RF/MW manufacturing to a contract manufacturer also can eliminate or reduce many costs that are less obvious and therefore sometimes not considered in the decision of whether or not to outsource. For example, by reducing the OEM's manufacturing headcount, outsourcing reduces the OEM's exposure to employment-related expenses and risks such as benefit costs, workers' compensation insurance, liability for accidents occurring on the

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- Capacitance: 10 nF

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- Orientation Insensitive
- One Piece Construction
- Insertion Loss: <0.5 dB typical</li>
- Operating Temperature: (-55°C to +125°C)
- RoHS Compliant Terminations

### 550L Series

- Case Size: 0402
- Operating Frequency:
   16 KHz (-3 dB roll-off) to 40+ GHz\*
- Capacitance: 100 nF

### **Applications:**

- High Speed Data
- Transimpedance amplifiers
- Broadband Test Equipment
- Broadband Microwave/ millimeter-wave
- ROSA/TOSA†
- SONET††



- \* 25 °C, no bias applied
- † Receive and Transmit Optical Sub-Assembly
- tt Synchronous Optical Network





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### Perspective

job and other potential legal liabilities, etc. Outsourcing manufacturing can also reduce or eliminate the need for administrative infrastructure required to support the manufacturing operation such as human resources, purchasing and accounting.

### **VALUE OF ONSHORE MANUFACTURING**

Countries such as China, Singapore, Thailand and Malaysia are often considered the obvious locations for RF/MW OEMs considering outsourcing to a contract manufacturer. Offering the advantages of low-cost labor and a rapidly developing manufacturing infrastructure, these and other developing countries have become the default location for companies wishing to outsource production in order to lower costs.

However, a combination of economic forces is eroding the cost advantages of developing countries while at the same time the United

States is becoming a more attractive place to build electronics products. A recent study from the Boston Consulting Group stated that: "Our analysis concludes that, within five years, the total cost of production for many products will be only about 10 to 15 percent less in Chinese coastal cities than in some parts of the U.S. where factories are likely to be built. Factor in shipping, inventory costs, and other considerations and - for many goods destined for the North American market - the cost gap between sourcing in China and manufacturing in the U.S. will be minimal."

But onshore outsourcing has advantages for RF/MW manufacturers that go beyond the general improvement in the U.S. competitive position. The highly complex nature of RF/MW manufacturing means that it is often difficult to completely document every aspect of what is required to produce a quality product and in some cases the requirements of the product are not even fully known. This leads to complexities in transferring a manufacturing process to a contract manufacturer. These complexities can be overcome; however, the unique nature of RF manufacturing can make it challenging to transfer an RF/MW process to an overseas contract manufacturer. Language difficulties may make it difficult to communicate the myriad of details needed to maintain the OEM's high quality standards.

The large physical distance between an overseas contract manufacturer and a U.S.-based OEM exacerbates these difficulties. It typically costs \$4,000 in travel expenses to send an employee to Asia for a short visit to a contract manufacturer. These costs do not include the costs of the employee's time. It takes a minimum of a week for an employee to fly to Asia, spend a day or two at the contract manufacturer, fly back and acclimate to the time zone changes, and resume his or her previous level of productivity. The time expended on such a trip by an engineer with a fully loaded cost of \$100,000 per year adds another \$2,000 to the cost. At a total cost of \$6,000 per visit, the OEM faces the difficult tradeoff between the need for close communications with the overseas contract manufacturer versus limiting trips to keep costs under control.





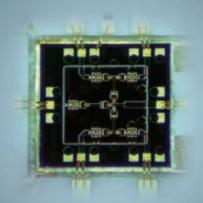
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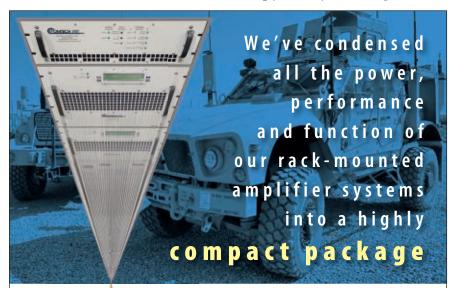
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### Perspective

When working with an overseas RF/MW contract manufacturer, it is also often necessary to ship U.S.-made equipment such as bonders and test equipment overseas. Shipping delicate equipment into developing countries is expensive, risks damage to the equipment and often takes months which can delay the product introduction.

Outsourcing RF/MW manufacturing to an onshore contract manufacturer also avoids other concerns and risks involved in working with an offshore source. The limited intellectual property protection in developing countries creates the risk that proprietary information provided by the OEM to an offshore contract manufacturer will later end up in the hands of a competitor. Working with an onshore contract manufacturer provides much greater protection of intellectual property rights and also makes it much easier to comply with any related regulations.



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### WHAT TO LOOK FOR IN A CONTRACT MANUFACTURER

Whether you are looking onshore or offshore, any credible RF/MW contract manufacturer should be able to provide complete fabrication and test capabilities including singulation, assembly, wire bond, test, repair, kitting and stocking of components. A quality system should be in place that assures the integrity of every product manufactured, such as compliance with ISO9001-2008, MIL-STD and J-STD requirements. Full RF test capabilities through 40 GHz and ITAR registration should be final tick boxes that will give you confidence there will be no bumps in the road to delivery. In the RF/MW field, a contract manufacturing company should also be able to demonstrate an ability to attract, retain and enhance the capabilities of a skilled staff such as wire bonders and die attach workers.

### BIG OR SMALL? WHAT'S RIGHT FOR YOU?

Bigger firms with large assembly lines are the obvious choice when high volumes and automation concerns are driving decisions. But even if these needs are the norm, the advantages of identifying at least one small local supplier cannot be overlooked. Their overhead expenses are lower so it does not require a specified minimum number of pieces per month. They generally work with OEMs on projects ranging from prototype builds to thousands of pieces per month and can scale up or down quickly to handle increasing volumes. They can easily switch gears and take on repair work or even a complete product line.

#### **CONCLUSION**

RF/MW manufacturing is considerably more difficult than conventional electronics manufacturing, so it requires skilled artisans with many years of experience to do it right. Many RF/MW OEMs are finding it difficult to maintain these resources internally or are finding their high cost makes it difficult to stay competitive. Onshore outsourcing makes sense for RF/MW products because it eliminates hidden costs and the time zone, language and cultural barriers that often make it difficult to transfer a process overseas.

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# Mobile World Congress Review

obile communication impacts the daily lives of hundreds of millions, drives commerce and shapes economies. The 2012 Mobile World Congress (MWC), which took place at the Fira de Barcelona Conference and Exhibition Centre between February 27 and March 1, has become an established global showcase for the industry and an important platform for the technology that is being developed today that will shape the future.

The GSMA reported that over the four days, a record number of more than 67,000 visitors (the number of individual attendees, including delegates, exhibitors, contractors and media) from 205 countries attended the Congress, with more than 1500 exhibiting companies occupying 70,500 net square metres of exhibition and business meeting space.

With such a worldwide audience, broad global issues other than the usual commercial proliferation of networks and services were addressed during the conferences, forums, seminars and GTI summit. For instance, recognizing that in emerging and developing regions, mobile communications technology has the capacity to provide lifelines, educate and be a tool for development, a number of seminars covered pertinent issues ranging from: green power for mobile and community power from

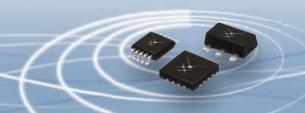
mobile, disaster response and agricultural value added services in emerging markets.

Of course, at a premier event that attracts global media attention and the participation of high profile movers and shakers, the major focus is on the need and desire to sate the developed world's rapacious appetite for mobile content and meet the challenge to develop applicable technology at a pace that will satisfy that demand.

The continuing evolution and promotion of the smartphone and now the 'superphone,' the mushrooming development of Apps for every purpose, the insatiable demand to download games, movies and live content and access the Internet, and even make the occasional old fashioned 'phone call' are putting an ever increasing strain on the networks. Capacity, or the lack of it, has been a major concern for some time. In recent years, considerable progress has been made, particularly at the 'core,' but the danger is that the problems have been moved to the fringes and, in this case, out of sight can mean out of range!

Only a few years ago, the new buzz at the Mobile World Congress was LTE, which, along

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SKY65535	WLAN Front-End Module with Integrated PA with Filter, LNA, and SPDT Switch	5.0	QFN 16L 2.5 x 2.5 x 0.45
SKY77701-16	High PAE Power Amplifier Module for CDMA / WCDMA / HSPA+ / LTE - Band I	1.92-1.98	10-pin MCM 3 x 3 x 0.9
WiEi Connectivity			

#### WiFi Connectivity

SE5516A	802.11ac Dual-Band Front-End Module with PA, LNA, and SP2T Switch	2.4, 5.0	LGA 4 x 4 x 1
SE5003L1	802.11ac Matched Power Amplifier with Harmonic Filter	5.0	QFN 20L 4 x 4 x 0.9
TT20P6-0709P0-1825E	High Power Infrastructure Filter can be Configured in a Pass Band Design	0.7–2.1	5" x 1.9" x 1"

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SKY13419-365LF	CMOS DBS Switch Matrix with Tone/Voltage Detector High Isolation 40 dB @ 900 MHz	0.25-2.15	QFN 20L 4 x 4 x 0.9
SKY65185	Dual-Channel Variable Gain Amplifier Front-End Module with 31.5 dB Control Range	1.7-2.7	32-pin MCM 7 x 7 x 1.35
SKY65373-11	Variable Gain Low Noise Amplifier with High Linearity @ 35 dB and Low NF @ 1 dB	1.7	16-pin MCM 8 x 8 x 1.3
SKY67130-396LF	High Linearity Amplifier Driver with +16 dBm OP <sub>1 dB</sub> and 39.5 dBm OIP3 @ 22 mA	0.7-2.7	DFN 8L 2 x 2 x 0.75
SKY73208	Wideband Rx Mixer with Integrated Integer-N PLL and VCO	0.35-5.0	36-pin MCM 6 x 6 x 1.35
SKYFR-000782	Single Junction Circulator with Very Low Insertion Loss of 0.08 dB Typical	2.11–2.17	Drop-in 19 mm
SKYFR-000827	Single Junction Circulator with Very Low Insertion Loss of 0.12 dB Typical	2.3–2.4	SMT – Robust Lead, 23 mm

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SE2436L	High Power 0.5 W Front-End Module for ISM band applications, with PA, LNA, Bypass and Antenna Diversity	2.4	QFN 24L 4 x 4 x 0.9
SE2438T	Ultra Low Power ZigBee® Front-End IC with PA, LNA, Tx/Rx Bypass	2.4	QFN 20L 3 x 3 x 0.5
SKY65367-11	High Power / High Efficiency Tx/Rx Front-End Module with Integrated PA and Bypass	0.17	16-pin MCM 4 x 4 x 0.9
SKY67012-396LF	Low Noise Amplifier with $<$ 0.85 dB NF and $<$ 5 mA Current @ 3.3 V	0.3-0.6	DFN 8L 2 x 2 x 0.75



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#### **Special Report**

with its siblings LTE-Advanced and TD-LTE, has developed at pace with rollouts having commenced. In particular, there have been significant deployments in Asia, particularly South Korea, while in North America, the spread has generally been confined to large cities with high density.

It also looks like LTE could finally find its voice. Major efforts are being made to provide Voice over LTE (VoLTE) – two years on from the GSMA announcing their backing of the 'One Voice' solution to VoLTE at the 2010 Mobile World Congress. Having been conceived as an IP cellular system solely for carrying data with voice carried either by VoIP or by 2G or 3G, operators have realised that the omission of voice from LTE, allied to the lack of SMS, needed to be addressed. Standardisation is now a key issue, with voice quality being a particular concern.

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Further along the developmental spectrum is 4G LTE-Advanced, a key feature of which is Carrier Aggregation, which is being standardized in 3GPP as part of LTE Release 10. Basically, carrier aggregation enables expansion of effective bandwidth delivered to a user terminal through concurrent utilization of radio resources across multiple component carriers that are 'aggregated' to form a larger overall transmission bandwidth. Work is ongoing but at MWC 2012, Cognovo demonstrated carrier aggregation communications in real-time on an LTE Advanced baseband, and a number of carriers have announced deployment as early as 2013.

Another approach to addressing the capacity question is the deployment of small cells to bridge the gaps and expand coverage. Some of the largest operators have made small cell deployments. 2012 has seen the world's first LTE femtocell deployment by SK Telecom and the marrying of small cell technology with Wi-Fi is a hot topic. Small cell developers stated that the current aim is to take advantage of chipset development and low cost components while employing advanced RF and network management.

As well as network capacity, another contagion of the smartphone revolution is the drain on handset batteries with the potential for 4G handsets requiring charging two or even three times a day. A specific answer to this problem is to address PA efficiency through the development and deployment of Envelope Tracking. This is a standard PA architecture providing power optimization technology which delivers high efficiency over the entire spectrum used for 3G and 4G standards. At MWC 2012, Nujira showcased its first commercial chip for mobile handsets.

With an event as vast and far reaching as MWC, it is impossible to cover all of the key issues and innovations and this article has attempted to highlight a few of the more significant areas of R&D. Many of these technological developments are in the RF and microwave sector with test and measurement, semiconductor and chipset, near-field communication, small cells and mobile backhaul companies demonstrating their latest offerings on the exhibition floor. For the full MWC wrap-up, visit www.mwjournal.com/MWC2012review.



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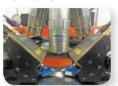
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# Techniques for Improving Noise and Spurious in PLLs

phase-locked loop (PLL) can be used for a range of purposes, including frequency synthesis. However, successful design of a synthesizer depends heavily on the choices the engineer makes, such as whether to employ a single or multiple loop approach, and on important design considerations like noise and spurious.

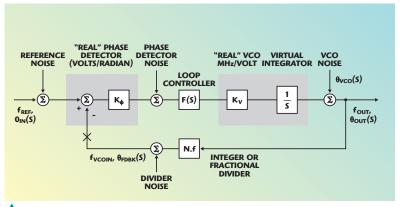


Fig. 1 A basic PLL block diagram is illustrated here with the various noise sources.

#### **UNDERSTANDING PLL BASICS**

In order to fully understand the choices and design considerations that come into play with the PLL, it is critical to first have an understanding of PLL basics. In the steady-state, a PLL is a linear control system where the variable of interest is phase. Laplace s-domain analysis is used to predict the stability and phase noise performance of the loop.

A basic block diagram of a PLL is shown in **Figure 1**. The "input" to the PLL is the reference frequency and the output frequency is  $f_{OUT} = N.f.f_{IN}$ . With an integer divider, the output frequency steps are the same as the reference. With a fractional divider, the output step size can be much less than the reference. However, fractional dividers have serious spur issues and the phase noise is typically not as good as integer dividers.

The open loop transfer function is the gain around the loop, GH(s). Analyzing GH(s) gives

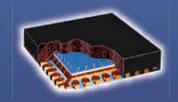
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Part Number	Freq. (GHz)	Insertion Loss (dB)	Peak Phase Error (°C)	RMS phase Error (°)	Input Power @1dB Comp
CHP3010-99F	1.2 - 1.4	7	-1 / +3	1.5	24
CHP3010-QFG	1.2 - 1.4	7	-1 / +3	1.5	24

#### S-BAND BARE DIE / SMT PLASTIC PACKAGE

Part Number	Freq. (GHz)	Insertion Loss (dB)	Peak Phase Error (°C)	RMS phase Error (°)	Input Power @1dB Comp
CHP4012a98F	2.7 - 3.5	6	-2 / +4	1	24
CHP4012-QEG	2.7 - 3.5	6	-2 / +4	1	24

#### C-BAND BARE DIE / SMT PLASTIC PACKAGE

Part Number	Freq. (GHz)	Insertion Loss (dB)	Peak Phase Error (°C)	RMS phase Error (°)	Input Power @1dB Comp
CHP4014-98F	5 - 6	6	-4 / +4	1	26
CHP4014-QEG	5 - 6	6	-4 / +4	1	26

#### X-BAND BARE DIE / SMT PLASTIC PACKAGE

Part Number	Freq. (GHz)	Insertion Loss (dB)	Peak Phase Error (°C)	RMS phase Error (°)	Input Power @1dB Comp
CHP3015-99F	8.5 - 11.5	7	-3 / +5	2	24
CHP3015-QDG	8.5 - 11.5	7	-	-	24

CMOS/TTL compatibility: 0 / 3.3 & 0 / 5.0 (V) - Switching time: <30ns (soon available in hermetic package)

#### L-BAND HERMETIC PACKAGE

Part Number	Freq. (GHz)	Insertion Loss (dB)	Peak Phase Error (°C)	RMS phase Error (°)	Control Voltage (V)
CHP6013-SRF	1.2 - 1.4	8.5	-5 / +5	2	-5 / 0



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#### **Technical Feature**

the stability information about the loop expressed as phase margin. The reference, phase detector and N divider noise obeys a lowpass transfer function where the loop rejects the noise beyond the loop bandwidth (BW). The voltage-controlled oscillator (VCO) noise obeys a highpass transfer function where the VCO noise is rejected inside the loop BW. The loop controller F(s) is typically an integrator with a zero, although more complicated networks can be used.

$$\begin{split} T_{\text{REF}}(s) &= \frac{\theta_{\text{OUT}}(s)}{\theta_{\text{IN}}(s)} = \frac{\text{Forward}\_\text{Gain}}{1 + \text{Loop}\_\text{Gain}} = \\ \frac{G(s)}{1 + \text{GH}(s)} \\ GH(s) &= \frac{\theta_{\text{FDBK}}(s)}{\theta_{\text{IN}}(s)} = K_{\phi} \cdot F(s) \cdot \frac{K_{\text{V}}}{S} \cdot \frac{1}{N} \\ LP(s) &= T_{\text{REF}}(s) = N \frac{GH(s)}{1 + GH(s)} \\ HP(s) &= T_{\text{VCO}}(s) = \frac{1}{1 + GH(s)} \end{split} \tag{1}$$

To model the noise associated with the various PLL components, the following equations can be used:

$$\mathfrak{L}(f) = (k_0 + \frac{k_1}{f} + \frac{k_2}{f^2} + \frac{k_3}{f^3})$$

$$S_{\phi}(f) = 2 \cdot L(f) = 2 \cdot (k_0 + \frac{k_1}{f} + \frac{k_2}{f^2} + \frac{k_3}{f^3})$$
(2)

Here, L(f) is the single-sideband (SSB) phase noise at a given offset from the carrier and  $S_{\varphi}(f)$  is the double-sideband phase noise or power spectral density. The coefficients  $(k_0,\,k_1,\,k_2,\,k_3)$  represent the noise floor 10 dB/decade, 20 dB/decade and 30 dB/decade regions. Lesson's model predicts that RF and  $\mu W$  oscillators have flat,  $1/f^2$  and  $1/f^3$  regions, while high Q oscillators (crystal and SAW) have flat, 1/f and  $1/f^3$  regions. Dividers and phase detectors have a flat and 1/f or flicker region. For example, for a  $\mu W$  VCO, knowing the floor, a point in the  $1/f^2$  region (dBf2 VCO, f2\_VCO) and a point in the  $1/f^3$  region (dBf3 VCO), the noise equation is obtained.

$$\begin{split} k_{0\_VCO} &= 10^{\frac{dB_{floor\_VCO}}{10}}; k_{2\_VCO} = 10^{\frac{dB_{f2\_VCO}}{10}} \cdot (f2\_VCO)^2; \\ k_{3\_VCO} &= 10^{\frac{dB_{f3\_VCO}}{10}} \cdot (f3\_VCO)^3 \\ S_{\phi\_VCO}(f) &= 2 \cdot (k_{0\_VCO} + \frac{k_{2\_VCO}}{f^2} + \frac{k_{3\_VCO}}{f^3}) \\ S_{\phi\_Input\_Noise}(f) &= S_{\phi\_REF}(f) + S_{\phi\_N\_Divider}(f) + S_{\phi\_PD}(f) \\ S_{\phi\_Input\_Noise\_Pedestal}(f) &= N^2 \cdot S_{\phi\_Input\_Noise\_Pedestal}(f) \cdot \left| LP(jf) \right|^2 \\ S_{\phi\_VCO\_Loop}(f) &= S_{\phi\_VCO\_Loop}(f) \cdot \left| HP(jf) \right|^2 \\ S_{\phi\_Output}(f) &= S_{\phi\_VCO\_Loop}(f) + S_{\phi\_Input\_Noise\_Pedestal\_Loop}(f) \end{split}$$

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Part Number	Frequency (MHz)	Gain (dB)	Pout (W)	Eff. (%)	Pulse Droop (dB)	Duty (%)	Pulse Width (µs)	VDD (V)	Dimension (mm)
RRP03250-10	135 ~ 460	31	300	45	0.5	10	200	50	114.3 x 25.4 x 28
RRP10350-10	1030 ~ 1090	28	350	50	0.5	5	200	50	53.2 x 28 x 8
RRP13330-10	1200 ~ 1400	14	330	65	0.5	20	500	50	85 x 40 x 10
RRP29280-10	2700 ~ 3100	9	280	50	0.5	20	500	50	86 x 39 x 10





#### kW SSPA

Part Number	Frequency (MHz)	Gain (dB)	Pout (W)	Eff. (%)	Pulse Droop (dB)	Duty (%)	Pulse Width (µs)	VDD (V)	Dimension (mm)
RRP131K0-10	1200 ~ 1400	53	1000	40	0.5	20	500	50	250 x 150 x 28
RRP291K0-10	2700 ~ 3100	60	1000	30	0.5	20	500	50	220 x 145 x 27



#### T/R Module

Part Number	Frequency (GHz)	Tx Pout (W)	Rx NF (dB)	Rx Gain (dB)	Tx Gain (dB)	Duty Cycle (%)	Pulse Width (µs)	Attenuator	Phase Shifter
RFUD95-X15-200	9.3 ~ 9.5	15	3.5	30	32	10	100	6 Bit, 31.5dB	N/A
RFUD31-STRM	2.7 ~ 3.5	200	3.5	25	53	20	500	6 Bit, 31.5dB	6 Bit, 360deg
RFUD13-LTRM	1.2 ~ 1.4	250	3.5	35	54	20	500	6 Bit, 31.5dB	6 Bit, 360deg



#### GaN Hybrid Amplifier

Part Number	Frequency (MHz)	Gain (dB)	Pout (W)	Eff. (%)	Pulse Droop (dB)	Duty (%)	Pulse Width (µs)	VDD (V)	Dimension (mm)
RRC13050-10	1200 ~ 1400	36	50	65	0.5	10	100	50	20.5 x 15 x 4.8
RRC29050-10	2700 ~ 3100	20	50	55	0.5	10	100	50	20.5 x 15 x 4.8
RRC31050-10	2700 ~ 3500	24	50	50	0.5	20	1000	50	20.5 x 15 x 4.8
RRY56025-10	5400 ~ 5900	20	25	42	0.5	10	50	50	20.5 x 15 x 4.8
RRC94030-10	9300 ~ 9500	17	25	40	0.5	10	100	50	20.5 x 15 x 4.8
RNP04006-A1	400 ~ 450	33	4	72	0.5	10	100	24	20.5 x 15 x 4.8





#### Radar LNA



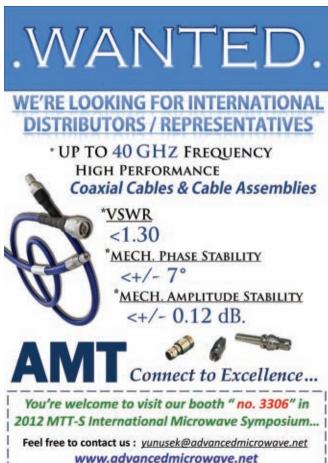


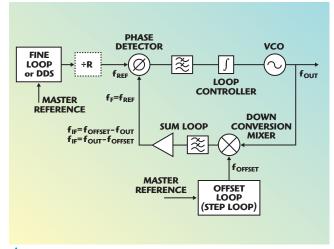
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▲ Fig. 2 Shown here is a common multiple-loop synthesizer configuration. Note that the loop to generate the master reference is not shown.

The input noise sources are then multiplied by N to produce what is commonly known as the pedestal. The optimum loop BW is where the pedestal crosses the VCO noise. The total noise is the sum of the loop modified pedestal noise (low passed) and VCO noise (high passed). Taking 10 log of the output noise, less 3 dB, gives the final SSB noise.

#### THE SINGLE-LOOP APPROACH

Single-loop phase-locked loops can be economical and efficient synthesizer solutions, offering a combination of moderate performance, compact size and low-power operation. Using commercial components such as fractional-N ASICs and careful modeling, they can be optimized to provide signals with reasonable phase noise, spurious performance and fine frequency resolution.

#### THE MULTI-LOOP APPROACH

The single-loop approach, however well optimized, has its limits. For higher performance synthesizers, multiple PLLs are used because they provide much better phase noise and spurs compared to simple, single-loop fractional N (FN) synthesizers. There are many configurations of multiple-loop synthesizers, one of which is depicted in *Figure 2*. It consists of a sum loop, fine loop and step loop.

The offset or step loop generates coarse frequency steps, while the fine loop (or DDS) generates a low-frequency, octave-wide signal with fine resolution that fills in between the coarse steps. The sum loop adds these two signals together. In general, the noise of the offset loop and master reference sets the "close-in" performance and the sum loop VCO sets the "far-out" performance. The fine loop should be a second-order contributor. Since the sum loop has a mixer, care must be taken with the frequency plan to avoid any spurs crossing within the loop BW.

This triple-loop approach is used in the Agilent N5181B/N5182B X-Series Signal Generator (see *Figure 3*). The fractional N loop generates 62.5 to 125 MHz. The 3 to 6 GHz output of the offset loop (125 MHz steps) is mixed with the sum loop VCO output frequency to produce an in-

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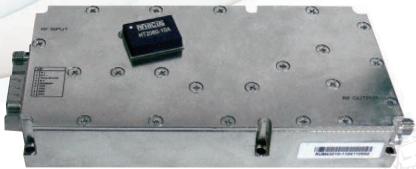


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#### Radar Application

The state of the s				
Part Number	Frequency (MHz)	Power (W)	Gain (dB)	PAE (%)
RRC13050-10	1200 ~ 1400	50	36	65
RRC31050-10	2700 ~ 3500	50	24	50
RRC29050-10	2700 ~ 3100	50	20	55
RRC94030-10	9300 ~ 9500	25	17	40
RRY56025-L1	5400 ~ 5900	25	20	42

#### Wideband Application

Part Number	Frequency (MHz)	Power (W)	Gain (dB)	PAE (%)
HM0005-10A	20 ~ 520	10	30	50
HM0525-10A	500 ~ 2500	10	20	35
TG2000-10	20 ~ 2000	10	14	45
TG2000-03	200 ~ 2000	3	33	45
TG2000-05	200 ~ 2000	5	33	38

#### Telecom Application

Part Numl		uency Powe	er Gain (dB)	PAE (%)
HT0808-1	5A 869 °	~ 894 10	35	55
HT2008-1	5A 2065 °	~ 2080 10	33	55
HT0808-3	0A 869 °	~ 894 25	28	45
HT1919-3	0A 1930 °	~ 1995       25	32	45
HT2121-3	0A 2110 °	~ 2170 25	33	45

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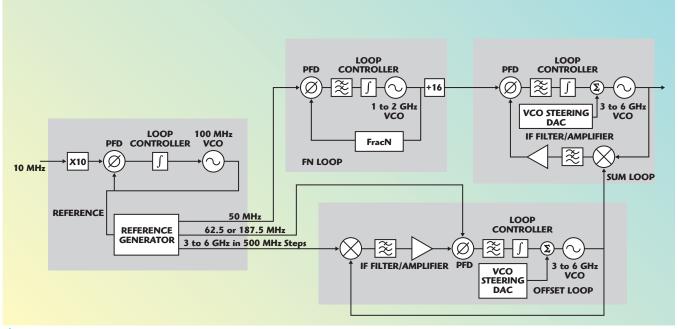
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termediate frequency (IF) that is the same as the FN loop generated reference. By using upper and lower sideband mixing, full coverage is obtained.

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From this 100 MHz, the 50 MHz reference for the FN loop is generated. For the offset loop, a series of frequencies from 3 to 6 GHz is generated in 500 MHz steps. Two additional reference frequencies of 62.5 and 187.5 MHz are generated for the offset loop.



📤 Fig. 3 This block diagram graphically depicts the triple-loop approach employed in the N5181B and N5182B X-Series signal generators.

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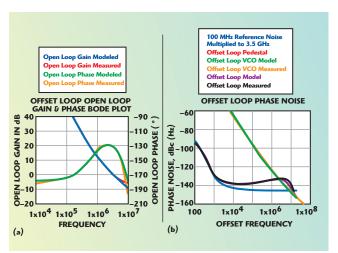
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▲ Fig. 4 The Bode and noise plots show excellent agreement between the model and measured results. The phase margin is ~48°.

and phase frequency detector noise. This assumes perfect multiplication of the 100 MHz VCXO signal to 500 MHz and then up to the various harmonics. A fudge factor is added to take into account any extra noise sources.

$$\begin{split} &S_{\phi\_Input\_Noise\_offset}(f) = n_{harm^2} \cdot S_{\phi\_500\_MHz}(f) + \\ &S_{\phi\_PD\_offset}(f) + S_{\phi\_62.5\_MHz\_Ref\_offset}(f) + S_{\phi\_fudge\_offset}(f) \end{split} \tag{4}$$

The 3 to 6 GHz VCO has rather poor phase noise. Consequently, the offset loop needs a wide-loop bandwidth to reject or track out the noise of the VCO. The offset loop controller consists of a differential lowpass filter, a low-noise differential to single-ended instrumentation amplifier, step attenuators to control the loop gain with changing  $K_{\rm V}$ . Each of these blocks, including the VCO tune port, adds phase shift in the loop that can adversely affect the phase margin and hence, the stability of the loop.

The differential lowpass filter rejects the 62.5 MHz energy from the phase detector so sidebands are not produced on the offset loop carrier. These sidebands can interact in the sum loop to produce a close-in spur on the final output. The trade off in designing this filter is to maximize the attenuation at 62.5 MHz while keeping the phase shift low at gain crossover. Within the passband of the filter, the phase shift can be approximated by a constant time delay.

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Gain Flatness:	±2.5d8 Typ.	Insertion Loss:	6.0dB Max.	Insertion Loss:	5dB Typ. (To 20GHz) 8dB Typ. (To 40GHz)
VSWR In/Out:	2.3:1	VSWR In/Out:	2.1:1 Typ.	VSWR In/Out:	2.5:1 Typ.
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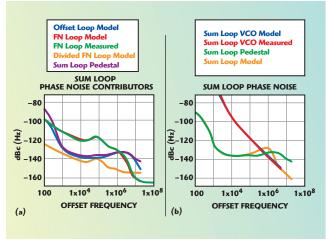
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The op-amp and VCO blocks are modeled with a simple time delay, T. The "lead lag" summing network was specifically designed to have flat attenuation with frequency. The gain crossover and open loop transfer function, assuming a delay of 24 nS, is shown in *Figure 4* and given by:

$$\begin{split} &f_{x\_offset} = K_{V\_offset} \cdot K_{\phi\_offset} \cdot A_{PD\_offset} \cdot \\ &A_{atten\_offset} \cdot A_{int\_offset} \cdot A_{Id \, lg\_offset} = 3.2 \,\, MHz \\ &T_{int\_offset}(s) = \frac{s + f_{z\_int\_offset}}{s} \, f_{z\_int\_offset} = 80 \,\, kHz \\ &Open \, Loop \, Gain \, (T_{offset} = 24 \,\, nS) \\ &GH_{offset}(s) = \frac{f_{x\_offset}}{s} \, T_{int\_offset}(s) \cdot e^{-2\pi \cdot s \cdot T_{offset}} \,; \\ &LP_{offset}(s) = \frac{GH_{offset}(s)}{1 + GH_{offset}(s)} ; HP_{offset}(s) = \frac{1}{1 + GH_{offset}(s)} \end{split} \label{eq:figet}$$

Using the lowpass and highpass loop transfer functions, and the various noise source equations, the offset loop noise can be calculated using:

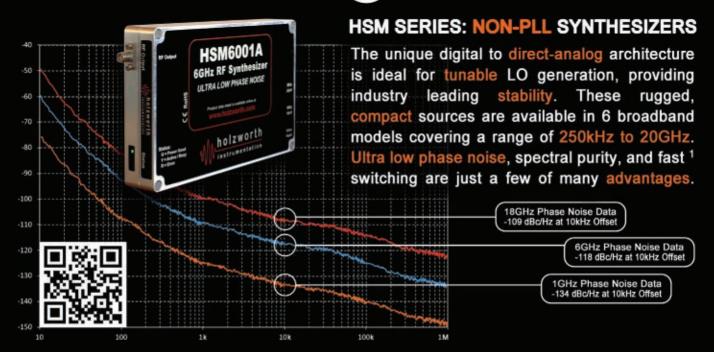
$$\begin{split} &S_{\phi\_{output\_offset}}(f) = S_{\phi\_{pedestal\_offset}}(f) \cdot \\ &\left| LP_{offset}(jf) \right|^2 + S_{\phi\_{VCO\_offset}}(f) \cdot \left| HP_{offset}(jf) \right|^2 \end{split} \tag{6}$$



lacktriangle Fig. 5 The plotted results of the sum loop noise contributors and final output noise.

The phase detector, reference and other noise sources in the loop degrade the multiplied reference noise by about 5 dB, total. The loop bandwidth is set at ~3.2 MHz. This causes a large phase noise peak, which is attenuated by the sum loop. The offset loop noise is shown in Figure 4.

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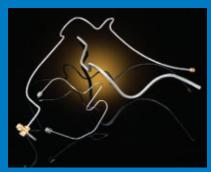
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#### FRACTIONAL N AND SUM LOOP

The FN loop generates a 1 to 2 GHz output that is divided by 16 to produce the 62.5 to 125 MHz reference input to the sum loop. The FN loop uses an Agilent proprietary chip set with a 50 MHz reference, making the noise and spurious performance much better than commercially available parts. Because of the division, the noise and spurs in the FN loop are reduced by 24 dB before the sum loop. The same methodology is used to analyze this loop. The 1 to 2 GHz output is divided by 16 to produce the 62.5 to 125 MHz before the input to the sum loop. The divided fractional spurs are less than –90 dBc.

The sum loop uses a low-noise 0.75 to 1.5 GHz VCO that is multiplied to 3 to 6 GHz. The reference input to the sum loop is the divided fractional N loop. The offset loop is summed using a mixer in the feedback path. Since the IF frequency of the sum loop (mixer output) is much less than the offset loop (mixer input), the mixer crossing spurs are high order and hence, at a very low level. The noise of the sum loop, as shown in *Figure 5*, is given by:

$$\begin{split} &S_{\phi\_pedestal\_sum}(f) = S_{\phi\_output\_offset}(f) + S_{\phi\_divided\_FN\_output}(f) + \\ &S_{\phi\_PD\_sum}(f) + S_{\phi\_fudge\_sum}(f) \\ &S_{\phi\_output\_sum}(f) = S_{\phi\_pedestal\_sum}(f) \cdot \left| LP_{sum}(jf) \right|^2 + \\ &S_{\phi\_VCO\_sum}(f) \cdot \left| HP_{sum}(jf) \right|^2 \end{split} \tag{7}$$

Using this mathematical software, it is easy to adjust the various loop parameters, such as gain crossover, pole and

zero locations, and the various noise sources in the loop to optimize performance by performing "what if" scenarios. Once this is done, the component values can be calculated and a circuit simulator used, like Agilent's Advanced Design System or SPICE, to verify each loop's performance with the component values in place.

#### **CONCLUSION**

Regardless of how well optimized a single-loop PLL is, there are still limitations. Multiple-loop solutions can substantially improve performance in terms of close-in and wide offset noise, along with spurious. Using the right design and modeling approaches, multi-loop PLLs can efficiently deliver the performance needed for demanding applications.

Eric Drucker is a senior engineer with Agilent's Technology Leadership Organization, a central resource for advancing measurement technology. He has been with Agilent for 12 years, working on PLL synthesizers for RF and microwave products and has taught numerous courses/workshops on PLL design. Prior to joining HP/Agilent, he spent the first half of his career with Fluke Corp. and several start-ups in the Seattle, Wash. area. He received his MSEE from Stanford in 1974.

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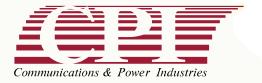
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# Improved Linearity Doherty Amplifier Using Tunable Offset Line

A Doherty power amplifier using a tunable offset line is proposed for linearity improvement. The conventional offset line is substituted with coupled lines and composite right/left-handed transmission lines (CRLH), incorporating a variable capacitance diode to adjust the phase at the output of the main amplifier, so the phase distortion of the peak amplifier at a high power level can be corrected by tuning the voltage of a variable capacitance diode in the proposed offset line. The performance of the proposed DPA is studied, using numerical simulations, in the frequency range from 2 to 2.5 GHz. The analysis indicates that the proposed DPA, with a tunable offset line, can show an improved linearity at a high input power. The measured results show an excellent IMD3, which agrees with the simulated results. Furthermore, compared to a conventional Doherty PA, the PAE of the proposed amplifier is improved by 5 to 7 percent, while the IMD3 is reduced by approximately 25 dB.

odern wireless communication systems, such as CDMA and W-CDMA, have critical system requirements for high linearity. Therefore, many power amplifiers are operated to deliver a significantly backed-off average output power. These methods result in low efficiency, due to the over 10 dB back-off. It is difficult to obtain optimum efficiency and high linearity performance in the same Doherty amplifier. The main linearity deterioration of Doherty amplifier occurs in the peaking amplifier, due to the peaking amplifier operating in Class C, which generates high order intermodulation distortion (IMD) products. Many traditional linearization techniques, such as pre-distortion and feedforward, could be adopted, but these methods require the use of external control circuits and signal processing, resulting in an increased

level of design complexity and its linear performance improvement is still limited. In addition, an N-way Doherty amplifier has also been reported for high efficiency and linearity; however, its size and performances have limitations for W-CDMA base station applications.

Composite right/left-handed transmission lines (CRLH) and capacitor-loaded coupled lines can suppress the second and higher order harmonics of the output<sup>1,2,3</sup> and at the same time, the structure exhibits either a negative or a positive phase, as well as a 0 phase, according to the design needs.<sup>4</sup> Due to its compact and

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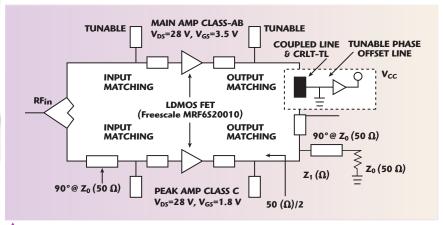


Fig. 1 Proposed architecture of a DPA using a tunable offset line.

flexible design, the structure lends itself easily to integration with other microwave components and devices. Recently, some works were reported to improve the linearity of Doherty amplifiers by composite right/lefthanded transmission lines and defected ground structure (DGS).<sup>5,6</sup> Because harmonic components play a positive role in improving PAE and linearity, the CRLH and DGS are used to suppress second and other order harmonics of the main amplifier output. However, at a high power level, the phase distortion of the peaking amplifier still cannot be solved, so the linear improvement is also limited. The inherent linearity deterioration of a Doherty amplifier sets a threshold for achievable performance.

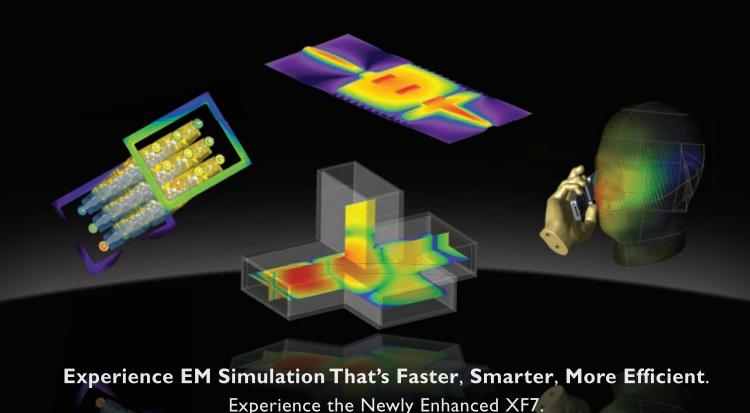
In this article, tunable CRLH and coupled lines, using a variable capacitance diode in an offset line to improve linearity performance of a Doherty amplifier, is introduced. The tuning voltage of a variable capacitance diode,7 the tunable CRLH and coupled lines, can be adjusted to adopt any phase and this makes the design more flexible and usable. The proposed structure is shorter by 7 to 12 mm in length than the offset line of a conventional one. The proposed structure suppresses the second and higher order harmonics of the main amplifier output and, at the same time, the phase distortion of the peaking amplifier at a high power level can be corrected by tuning the voltage of a variable capacitance diode in CRLH and coupled lines. The proposed tunable offset line method not only fulfills the phase delay and phase correction, but also results in some other improvements, such as higher PAE and improved linearity.

#### **FUNDAMENTAL THEORY**

#### **Circuit Description**

In the proposed tunable Doherty amplifier, the conventional offset line is replaced with a variable capacitance diode loaded CRLH and coupled lines to suppress the harmonics and adjust the phase with the variable capacitance diode. The proposed structure makes the design more flexible and makes many other improvements in the Doherty amplifier. The topology of the circuit is shown in *Figure 1*. The main amplifier (Class AB) signal, passing through a tunable offset line and a  $\lambda/4$  transmission line, is combined with the peak power amplifier (Class C) signal at the output. Due to the Class AB of the main amplifier, the linearity of the entire Doherty amplifier is ensured and, at the same time, with the peak amplifier operating in Class C, the efficiency of the entire Doherty amplifier also is improved. The tunable offset line consists of variable capacitance diode-loaded coupled lines or variable capacitance diode-loaded CRLH. The R<sub>opt</sub> and Z<sub>0</sub> are used for the load impedances of the main and peak amplifiers, respectively. The  $R_{opt}$  is selected as  $2Z_0$  for matching and decreasing power leakage to the peak amplifier when the peak amplifier is turned off, and when it is turned on, Z  $_0$  is 50  $\Omega$  and Z  $_1$  is  $\sqrt{Z_0\,\frac{Z_0}{2}}\Omega$ 

Figure 2 shows a tunable offset line using variable capacitance diodeloaded coupled lines. The structure consists of a variable capacitance diode load and a pair of the symmetrical parallel coupled-lines. The harmonic suppression and variable phase are



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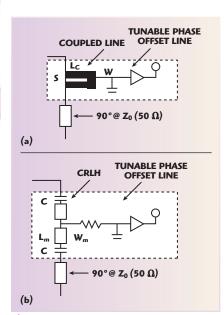


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▲ Fig. 2 Proposed offset line using variable capacitance diode-loaded coupled lines (a) and using variable capacitance diode-loaded CRLH (b).

achieved by the variable capacitance diode loaded coupled lines. The impedance of the tunable offset line is  $50 \Omega$ , and the phase of the offset line can be modified through changing the voltage of the variable capacitance diode. The modifying phase of the main power amplifier will be more flexible, so that the phase distortion of the peaking amplifier at high-power level will be cancelled. Therefore, the performance of the proposed Doherty power amplifier (DPA) can be improved much more than with a DPA using a conventional offset line. The other tunable offset line is a variable capacitance diode loaded CRLH. The variable capacitance diode-loaded CRLH replaces the conventional offset line, where the right-handed transmission line (RHTL) and the left-handed transmission line (LHTL), are composed of capacitors and inductors. When the series and shunt resonances are equal, the structure is said to be balanced. According to the desired phases for two different frequencies, the phase response of CRLH-TL will be  $-\pi/2$  at  $f_1$  (fundamental frequency) and  $-2\pi$ at f<sub>2</sub> (second harmonic). Therefore, a large portion of the second harmonics generated from the main and peaking amplifiers will be cancelled at the summing load. Furthermore, at highpower level, the phase distortion of the peaking amplifier will be corrected through the tuning voltage of the variable capacitance diode.

#### **Linearity Analysis**

At low-power level, the IMD3 of the entire DPA is only provided by the main amplifier, while the peak amplifier is turned off, due to the suppression of harmonics at the output of the main amplifier in the proposed DPA. Compared to the conventional offset line structure, the second and higher order harmonics of the main amplifier are effectively suppressed from 3.5 to 7 GHz by the proposed structure. The AM-AM distortions of the proposed DPA are lower than that of a conventional DPA.

At high-power level, while the peak amplifier is turned on, IMD3 is a composite of contributions from both the main and peak amplifiers, the output phase distortion of the Doherty amplifier comes mainly from the peak amplifier, while the carrier amplifier is biased at Class AB operation. In this case, the nonlinear output current of the active devices can be approximately expressed by a Taylor series expansion:

$$I_{out} = gm_1v_i + gm_2v_i^2 + gm_3v_i^3 + \dots$$
 (1)

where v<sub>i</sub> is an input voltage and gm<sub>v</sub> is the xth-order expansion coefficients of the nonlinear transconductance. The third-order intermodulation distortion (IMD3) current is mainly generated by the gm<sub>3</sub>v<sub>i</sub><sup>3</sup> term of Equation 1. Assuming that the load modulation does not seriously affect linearity and that the main amplifier is biased as Class AB to have a gm<sub>3</sub> of -a, the bias of the peaking amplifier for the twoway Doherty amplifier should be adjusted to have a gm<sub>3</sub> of a to perfectly cancel the IMD3 current generated by the main amplifier. However, the bias point of the peaking amplifier for a perfect IMD3 cancellation may approach closely to a Class B bias. Furthermore, a Class C biased peak amplifier brings a lot of AM-AM and AM-PM distortion at high power. The AM-AM and AM-PM distortions of the peak amplifier can result in IMD3 deterioration. However, in the proposed DPA, the phase distortion of the peak amplifier can be corrected by tuning the phase of the main amplifier, so that the phase distortion and gm<sub>3</sub> of the proposed entire DPA can be decreased. Therefore, the IMD3 of the entire DPA is improved. In



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CT-3838-N	5 Kw Pk 500 W Av	N Conn.	2.7-3.1 GHz
CT-1645-N	250 W Satcom	N Conn.	240–320 MHz
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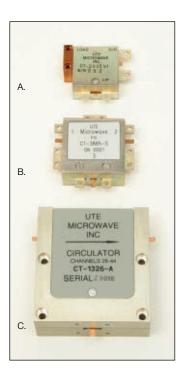
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the proposed DPA, tuning the variable capacitance diodeloaded coupled lines or the variable capacitance diodeloaded CRLH at the output of the main amplifier can correct the phase

distortion of the peak amplifier. At the same time, the second and higher order harmonics of the main amplifier output are largely suppressed, so the linearity of the proposed DPA is improved.

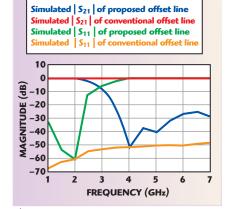
#### REALIZATION OF THE LINEAR AMPLIFIER BASED ON A TUNABLE OFFSET LINE

### Tunable Varactor Diode-loaded Coupled Lines for Offset Line

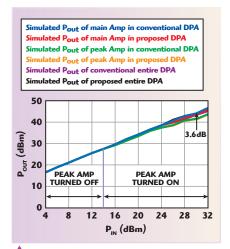
The schematic diagram of a tunable offset line, using varactor diode-loaded coupled lines, was shown previously. The tunable offset line consists of a variable capacitance diode load and a pair of symmetrical parallel coupledlines with a length  $L_c$ , a width W and a slot S between the lines. The phase of the offset line varies according to changes in capacitance of the diode, which are obtained by tuning the reversed voltage of the diode. The reactance and variable phase of the proposed structure are shown in **Table 1** for the frequency range from 2010 to 2100 MHz, where, L<sub>c</sub>, S and W are 4, 0.2 and 0.5 mm, respectively. C<sub>s</sub> is the equivalent value of the varactor diode. In addition, a 50  $\Omega$  tunable offset line is chosen to match the  $\lambda/4$  transmission line. The simulated S-parameters of the varactor diode-loaded coupled lines and the conventional offset line are shown in Figure 3, compared to a conventional offset line. The second and higher order harmonics in the varactor diode-loaded coupled lines is largely suppressed. The rejection band is extended from 3.5 to 7 GHz with a rejection ratio more than 20 dB. In the total process of DPA operation (low and high power level), the linearity of the main amplifier, and also of the overall Doherty amplifier improved, due to the suppression of the second and higher harmonics at the main amplifier output in the proposed structure. The optimized performances are shown on the basis of a 23.2° offset line.

Figures 4 and 5 show the simulat-

TABLE I					
REACTANCE AND PHASE OF THE PROPOSED STRUCTURE					
Reverse Voltage (V)	C <sub>s</sub> (PF)	Reactance	Phase		
1.8	10.0	49.9 ∠0.03	-21.4°		
1.0	12.0	49.9 ∠0.01	-23.1°		
0.6	15.0	50.1 ∠0.03	–25.6°		



▲ Fig. 3 Simulated S-parameters of the varactor diode-loaded coupled lines and conventional offset line.



▲ Fig. 4 Simulated AM-AM distortions in DPA using a tunable coupled line and a conventional DPA.

ed AM-AM and AM-PM distortions of the proposed and conventional DPAs. At low-power level, the IMD3 of the entire DPA is only provided by the main amplifier, while the peak amplifier is turned off. The phase distortion in the conventional DPA is almost the same as that of the proposed DPA. Due to the suppression of harmonics in the output of the main amplifier in the proposed DPA, the AM-AM distortions in the proposed DPA is lower than that of a conventional DPA. At high-power level, while the peak amplifier is turned on, IMD3 is



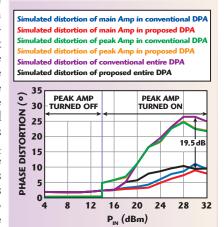
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a composite of the contributions from both the main amplifier and peak amplifier. The harmonics of the main amplifier are suppressed by the proposed coupled line. While P<sub>in</sub> is 30 dBm, the P<sub>out</sub> distortion of the proposed DPA is improved by as much as 3.6 dB over that of the conventional DPA. Furthermore, high-power level, the phase distortion of the peak



▲ Fig. 5 Simulated AM-PM distortion in DPA using a tunable coupled line and a conventional DPA.

amplifier (Class C) is large, which will result in the deterioration of IMD3. However, the gm<sub>3</sub> parameters of the FETs are opposite in the peak and main amplifiers of the proposed DPA. The phase distortion of the peak amplifier can be corrected by tuning the phase of main amplifier, so that the phase distortion and gm<sub>3</sub> of the proposed entire DPA can be decreased. Therefore, the IMD3 of the entire DPA is improved. In the proposed DPA, tuning the reversed voltage of the varactor diode-loaded coupled lines

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at the output of the main amplifier can correct the phase distortion of the peak amplifier. As shown, the simulated AM-PM distortion is improved in the proposed DPA, especially, when  $P_{\rm in}$  is 30 dBm, the phase distortion of the proposed DPA is improved by 19.5° over that of a conventional DPA.

#### **Tunable Varactor Diode-loaded CRLH for Offset Line**

To achieve the tunable offset line, a variable capacitance diode-loaded CRLH can also be adopted. The configuration of the proposed offset line was shown previously. The proposed structure is composed of a varactor diode and CRLH. The CRLH is realized by loading a conventional transmission line (TL) with lumped element series capacitors (C) and shunt inductor (L) where the length and width of the right-handed transmission line in CRLH are  $l_{\rm m}$  and  $w_{\rm m}$ , respectively. When the series and shunt resonances are equal, the structure is said to be balanced,  $Z_{\rm OR}$ ,  $Z_{\rm OL}$  and  $Z_{\rm o}^{\rm CRLH}$  are fixed as  $Z_{\rm offset}$ . The characteristic impedance of the tunable offset line and the  $\lambda/4$  transmission line can be obtained by a load modulation technique. The CRLH can be designed using P and Q, where P and Q are

$$2\pi\sqrt{L_{_{R}}C_{_{R}}}$$
 and  $\frac{N}{2\pi\sqrt{L_{_{C}}C_{_{C}}}}$ 

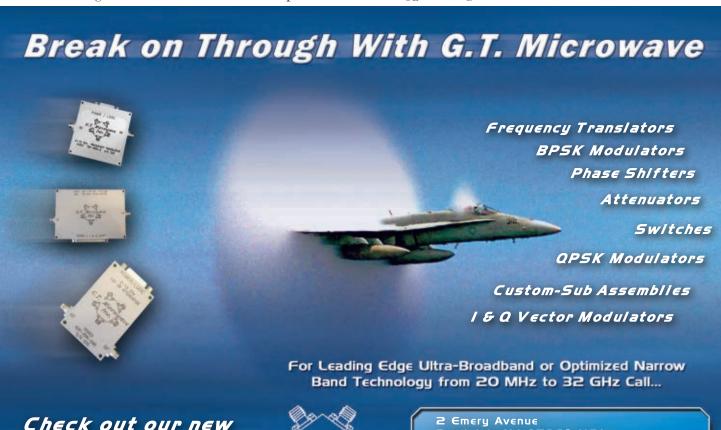
respectively. The RH TL has a negative phase response (phase lag) proportional to  $\sqrt{L_RC_R}$ , whereas the LH TL has a positive phase response (phase lead) proportional to  $1/\sqrt{L_CC_C}$ . P, Q,  $Z_{OR}$  and  $Z_{OL}$  are altogether used to determine C, L and the

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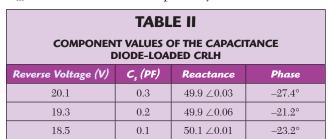
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physical length of RH-TL. When C and L are  $10\,\mathrm{pF}$  and  $42\,\mathrm{nH}$ , and  $l_\mathrm{m}$  and  $w_\mathrm{m}$  are 4 mm and 1 mm, respectively,

the reactance and variable phase of the proposed structure is shown in **Table 2**, in the frequency range from

2010 to 2100 MHz. Because the second harmonics generated in the main and peaking amplifiers will be cancelled at the summing load, while the peak amplifier is turned off, harmonics cannot be

suppressed, so the linearity is not improved. At high-power level, the peak amplifier is turned on when the main amplifier reaches saturation, tuning the reversed voltage of varactor diodes in CRLH, the phase distortion of the peak amplifier at high-power level can be corrected. As shown in *Figure* 6, at high-power level, compared to a conventional Doherty PA, the simulated AM-PM distortion of the proposed Doherty PA is reduced by 12.3 dB (P<sub>in</sub> is 31 dBm).





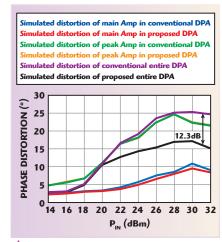
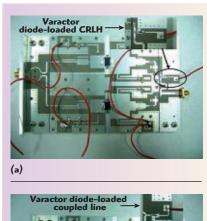
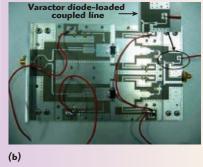


Fig. 6 Simulated AM-PM distortion in DPA using tunable CRLH and a conventional DPA





▲ Fig. 7 Photographs of DPAs using a varactor diode-loaded CRLH (a) and coupled lines (b).



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#### SIMULATED AND MEASURED RESULTS

The proposed Doherty power amplifier was simulated using Agilent ADS from 2 to 2.5 GHz. **Figure 7** shows the photographs of the fabricated proposed Doherty amplifiers (varactor diode-loaded CRLH and varactor diode-loaded coupled line), where a Taconic RF35 substrate ( $\epsilon_r$  = 3.5 tan  $\delta$  = 0.001) was used. The Microsemi's KV2111 and Philips's BB181 varactor diodes are chosen for

the tunable coupled line and tunable CRLH, respectively. The phase of the offset line is tuned at  $-21^{\circ}$ ,  $-23^{\circ}$  and  $-27^{\circ}$  by adjusting the voltage of the varactor diode manually. The optimized PAE and linearity is achieved with a  $-23^{\circ}$  phase offset line. The PAE of the DPA is simulated by using load/source pull and harmonic balance methods. The PAE is measured by calculating  $P_{ac}/P_{dc}$ , where  $P_{ac}$  is the difference between  $P_{out}$  and  $P_{in}$ .  $P_{dc}$  is calculated from the voltage and

current of the power supply. At highpower level, a better match at the output of the main amplifier is achieved and at the same time, the parameter y is optimized using the tunable offset line, so the total efficiency of the Doherty amplifier system is improved. The measured and simulated PAEs of the proposed DPA and conventional PDA are shown in Figure 8. At lowpower level ( $P_{out}$  under 29 dBm), the peak amplifier is turned off and the PAE of the proposed DPA is the same as that of the conventional DPA. For  $P_{out}$  above 29 dBm, the peak amplifier is turned on and the voltage of varactor diode is adjusted to optimize the match and compensating phase. Consequently, the PAE of the proposed DPA is improved. The measured and simulated PAE of the proposed DPA is greater (5 to 7 percent) than that of the conventional DPA. The maximum measured PAE of the proposed DPA is 45.2 percent at 2.01 GHz.



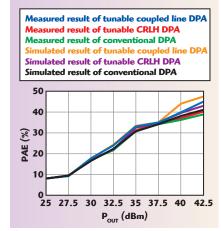
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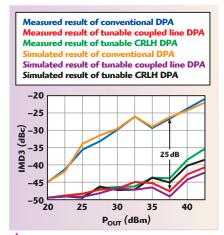
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▲ Fig. 8 Measured and simulated results (PAE) of the proposed DPA and conventional DPA.



▲ Fig. 9 Measured and simulated IMD3 of the proposed DPA and conventional DPA.



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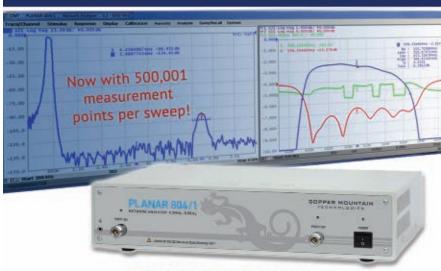
Figure 9 shows the measured and simulated IMD3 performance of the proposed DPA using two-tone signals at 2015.5 and 2020.5 MHz (the tone spacing is 5 MHz). In the proposed DPA, the harmonic of the amplifier is suppressed. At the same time, the phase distortion of the peak amplifier and gm<sub>3</sub> of the proposed entire DPA can be decreased by tuning the proposed offset line, so the IMD3 of the two proposed DPAs were considerably improved compared to that of

the conventional DPA. The IMD3 of the DPA using the tunable CRLH is not as good as that of the DPA using a tunable coupled line, mainly because the harmonic of the DPA cannot be suppressed while the peak amplifier is turned off and the phase of the second harmonic deviates a little from  $-2\ \pi,$  while tuning the tunable offset line at high-power level. At low-power level ( $P_{out}$  under 29 dBm), the peak amplifier is turned off and the harmonic of the main amplifier is suppressed by

the proposed structure. IMD3 is improved over that of the conventional one. At high-power level ( $P_{out}$  above 29 dBm), the peak amplifier is turned on, the phase of main amplifier and gm<sub>3</sub> are modified by tuning the voltage of the varactor diode and the distortion of the peak amplifier output is corrected. The IMD3 is improved by approximately 25 dB better than that of a conventional one. The data shows the improvement in linearity due to lower harmonics and the decrease of the phase distortion and gm<sub>3</sub>.

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#### CONCLUSION

A Doherty power amplifier, using a tunable offset line, is proposed to improve linearity and PAE. The tunable offset line is achieved by two structures, one is a varactor diode loaded coupled line, the other is a varactor diode-loaded CRLH. The proposed structure is utilized to suppress second and higher order harmonics and, at the same time, it can correct the phase distortion of the peak amplifier and decrease the gm<sub>3</sub> of the entire DPA by tuning the voltage of the varactor diode at high-power level. In addition, tuning the phase in a DPA becomes more flexible with the proposed structure. Testing results show that the linearity of the proposed DPA has been improved by 25 dB over the conventional DPA, which verifies the advantages of the proposed structures.

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# Global Navigation Satellite Systems and Their Applications

The Global Positioning System (GPS) was once the only operational global navigation satellite system (GNSS) and it was used all over the world to access location-based services (LBS). With the Russian GLONASS navigation system and the future deployment of China's Compass and Europe's Galileo navigation, there will be increased focus on the capabilities and applications of such systems. This article gives an overview of the different navigation systems, explains the navigation channel and generic approach used by a commercial standard receiver to calculate a user position and generally describes channel acquisition and tracking. GNSS applications such as differential GNSS (D GNSS) and multiple frequency-band navigation, their complexity and benefits are also presented.

lobal navigation satellite systems are made up of satellites spanning the globe in a set of defined orbits and aim to provide accurate, uninterrupted and global three-dimensional (3D) position and velocity information to users equipped with appropriate receiving equipment. GPS has been operational for some time and GLONASS has just become operational, whereas Galileo and Compass navigation systems will be deployed gradually in the next ten years and may be used in addition to GPS to improve location-based services.

A GNSS network is composed of satellite space vehicles (SV), user equipment (UE) and

control stations (CS). Satellite transmissions are referenced to highly accurate atomic clocks onboard the satellites that are synchronous to the GNSS system time base.

The worldwide control network monitors the health and status of the satellites and uploads the satellite navigation data, which is composed of immediate 'ephemeris' navigation data and non-immediate 'almanac' navigation data from different CSs. This data, along with the ranging information tracked at the UE

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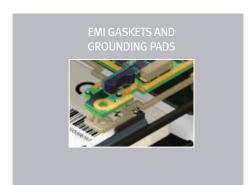




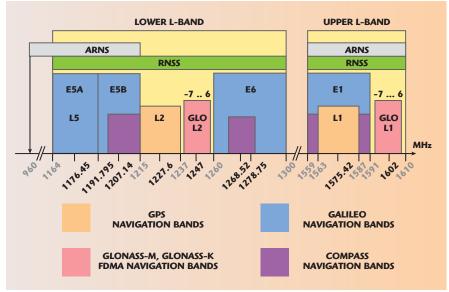
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#### **Technical Feature**



▲ Fig. 1 GNSS navigation RF bands.

from at least four satellites, enables the receiver module to calculate the satellites' positions and subsequently the 3D position of the UE.

#### **GPS**

The nominal GPS satellite constellation consists of 24 middle earth orbit (MEO) satellites arranged in six orbital planes with four satellites per plane. The satellites broadcast ranging codes and navigation data on three frequencies - L1 (1,575.42 MHz), L2 (1,227.6 MHz) and L5 (1,176.45 MHz) - using code division multiple access (CDMA), as can be seen in Figure 1. Each satellite transmits on these bands, but with different ranging codes than those employed by other satellites. These codes were selected because they have low crosscorrelation properties, thereby minimizing the interchannel interference.

#### **GLONASS**

GLONASS is a frequency division multiple access (FDMA)-based GNSS. A subcarrier is allocated but not reserved to a specific satellite. GLONASS became fully operational at the end of 2011, when the three nominal orbital planes were completely filled by eight satellites each. All satellites additionally share one spreading code that is optimized for noise suppression. Two satellites can share the same frequency number if they are located at diametrically opposite antipodal points on the same orbit, and therefore cannot be seen

by a user on the Earth at the same time. Subcarriers are allocated to GLONASS in the upper and lower bands.

The modernization of GLONASS as part of the GLONASS-K program will be continued. In the future, Russian satellites are to broadcast optimized CDMA signals in the GPS and Galileo L1/E1 bands as well as in other bands, in order to harmonize the GLONASS system with GPS and Galileo.

#### **GALILEO**

Galileo is an independent European GNSS. It is expected to be partially operational with 18 satellites in 2015 and fully operational with 30 satellites in 2020. One of the benefits of Galileo is that it can complement GPS to provide better navigation performance mainly in urban areas. The system uses CDMA to modulate the satellite signals and thus employs a dedicated spreading code for each space vehicle.

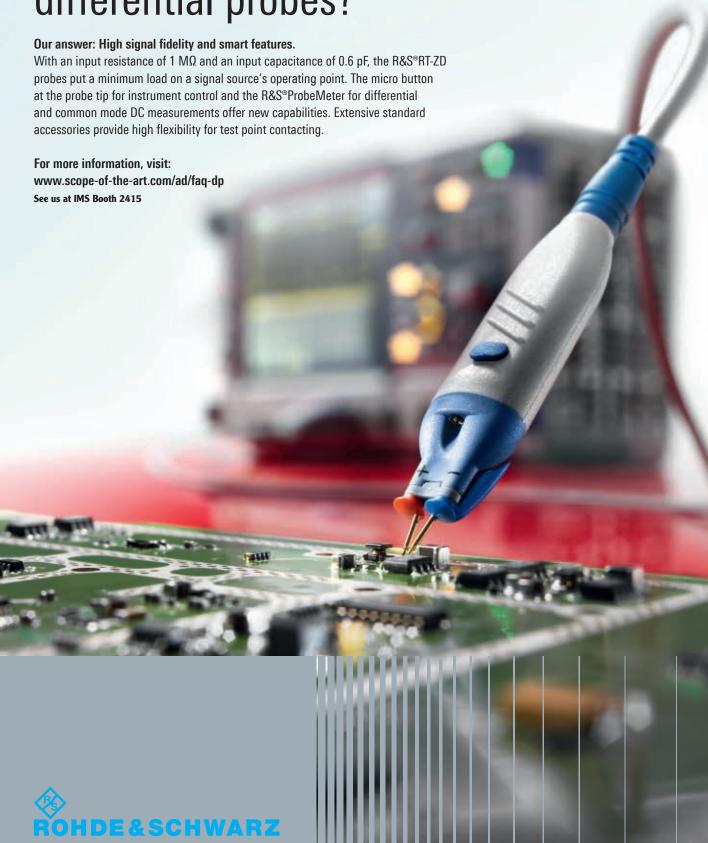
In addition, GPS and Galileo are supposed to share the same frequencies in the upper GNSS band (also called L1/E1) and minimize inter/intrasystem interference by selecting orthogonal pseudo random noise (PRN) and applying binary offset carrier (BOC) modulation, as shown in *Figure 2*.

#### **COMPASS**

Compass is a global navigation system that will not be fully operational before 2020. Because the Galileo proj-

### Your question:

## What's important about differential probes?



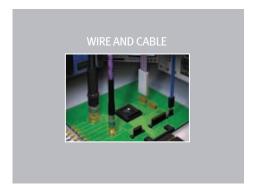
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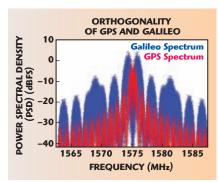
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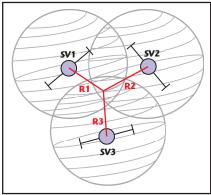
▲ Fig. 2 Power spectral density of GPS L1 C/A and Galileo E1.

ect has been delayed, China's regional Compass satellite system Beidou-2, designed to cover large parts of Asia, is scheduled to become operational in 2012 and broadcast on the same bands pre-allocated to Galileo (see Figure 1). These bands can then be acquired solely by the Chinese Compass/Beidou-2 navigation program.

#### **LOCALIZATION SYSTEM MODEL**

Navigation employs ranging to determine a user's position. Therefore, taking ranging measurements from different satellites (which may belong to different navigation satellite systems) makes 3D positioning possible. The geometric range, R<sub>i</sub>, is defined as the line of sight (LOS) distance from the satellite to the user. Knowing the position of three satellites and the absolute geometric range at a given UE location from each satellite allows users to locate their position at the intersection of three spheres centered around the satellites, each having a radius, R<sub>i</sub>. This basic trilateration approach is illustrated in Figure 3.

The geometric range R<sub>i</sub> (equivalent to LOS propagation) is not actually available at the UE, since the satellite signal propagation time gets distorted due to different factors such as refraction in the ionosphere and the troposphere, multipath propagation and satellite clock ambiguities. The distorted version of the geometric range is the pseudorange p<sub>i</sub>, which is the distance crossed by the ranging signal of a specific satellite to reach a user on the Earth. If ti is defined to be the propagation time of the GNSS signal from  $sv_i$  to the UE, then  $p_i = t_i c$ , where c is the speed of light. The ranging observation t<sub>i</sub> and consequently p<sub>i</sub> can be directly calculated from the tracked code and carrier phase of the corresponding tracking channel at the



▲ Fig. 3 Illustration of localization using ranging signals from three satellites.

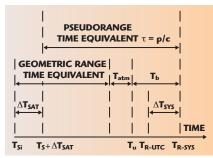


Fig. 4 Illustration of satellite-UE channel model.

UE. The navigation solution based on the aforementioned trilateration concept requires resolving the ambiguity in the pseudorange of every tracked satellite and thereby calculating  $R_i$  using the indirectly measured  $p_i$  and the GNSS satellite-UE channel model that relates  $R_i$  to  $p_i$ .

#### GNSS SATELLITE-UE CHANNEL MODEL

As shown in *Figure 4*, the generic channel model that can be used to relate the geometric range to the pseudorange SV<sub>i</sub> of space vehicle can be expressed as:

$$\begin{split} p_{_{i}} &= \tau_{_{i}}c = \\ R_{_{i}} &+ (T_{atm_{_{i}}} + T_{_{b}} - \Delta T_{SAT_{i}})c \end{split} \tag{1} \end{split}$$

where  $T_b$  corresponds to the receiver time bias,  $T_{atm}$  to the atmospheric ambiguities and  $\Delta T_{SAT_i}$  to the satellite clock errors. The geometric range  $R_i$  of a satellite (the radius of the trilateration sphere) can be calculated from the observed  $t_i$  using Equation 1. The UE location is determined by calculating the geometric range of at least four satellites and the corresponding satellite coordinates  $(x_i, y_i, z_i)$ , which are the centers of the trilateration spheres at  $T_{si}$ , where

### Your question:

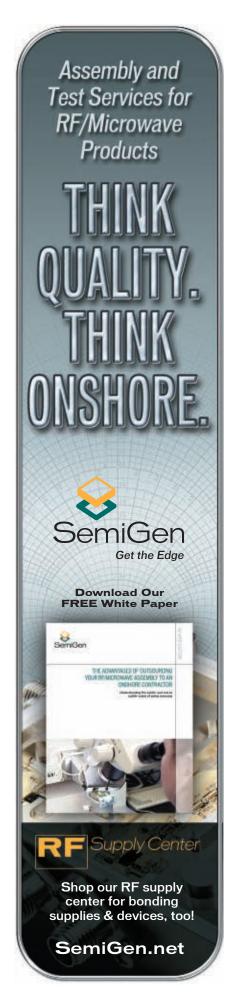
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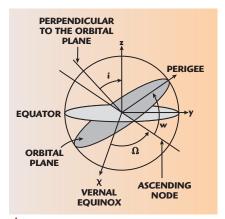


Fig. 5 Satellite's position in ECI.

$$T_{\scriptscriptstyle Si} = T_{\scriptscriptstyle R-UTC} + \Delta T_{\scriptscriptstyle SYS} - \tau_{\scriptscriptstyle i} - \Delta T_{\scriptscriptstyle SAT_i} ~~(2)$$

 $T_{\rm SYS}$  is the time difference between a specific GNSS system time base and a common system time base for the Universal Time Coordinate (UTC) to be calculated and  $T_{\rm R-UTC}$  corresponds to the receiver time in UTC.

Least square algorithms are usually used for UE location and time calculation. Other weighted least square algorithms with weights assigned proportionally to the measured carrier-to-noise ratio (C/N) of every tracked satellite are also very widely used in commercial receivers.  $T_{\rm b},~T_{\rm atmi}$  and  $\Delta T_{\rm SAT_i}$  are the distortion parameters that differentiate the geometric range from the pseudo range and will be described in the following subsections.

#### SATELLITE POSITION CALCULATION

To determine the location of the UE, first the position of all satellites must be determined. According to Newton's laws, the gravitational force exerted by the Earth's mass M on a satellite of mass m located at a distance r is:

$$\mathbf{F} = \mathbf{m}\mathbf{a} = -G\frac{\mathbf{m}\mathbf{M}}{\mathbf{r}^3}\mathbf{r} \tag{3}$$

G is the universal gravitational constant; r is the distance between the center of gravity of the Earth and the satellite in an Earth-centered inertial (ECI) orthonormal xyz coordinate system whose x and y axes do not rotate with the Earth. In Equation 3,  $\mathbf{r} = \|\mathbf{r}\|$ . The transformation from the differential equation's ECI coordinate system to the UE coordinate system, which

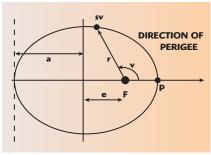


Fig. 6 GNSS orbital parameters.

rotates with the Earth and is also called an Earth-centered, Earth-fixed (ECEF) system, is merely a rotation.

Equation 3 should be rotated from ECI to ECEF to obtain a differential equation that can be used to calculate the satellite coordinates in the same UE's ECEF coordinate system. Only then can the trilateration generic concept work properly.

#### **ECI VS. ECEF**

The ECI coordinate system is centered at the Earth's center of gravity. The xy plane is taken to coincide with the Earth's equatorial plane. As described in Kaplan¹ (section 6), GPS ECI uses the orientation of the equatorial plane at 12:00 UTC on January 1, 2000. The x-axis is fixed in the direction of the vernal equinox (see *Figure 5*). The z-axis is normal to the xy plane.

ECEF, on the other hand, is the coordinate system used to calculate the position of UE, since it rotates with the Earth. The x-axis points in the direction of 0° longitude. Therefore, the transformation between ECI and ECEF is a rotation of the xy plane. The angle of rotation is derived from the Earth's sidereal time at any given moment.

#### **MOTION EQUATION**

The acceleration vector **a** in Equation 3 is the second derivative of **r**. Consequently, the two-body mass differential equation of motion in ECI is:

$$\frac{\mathrm{d}^2 \mathbf{r}}{\mathrm{dt}^2} = -\frac{\mathrm{GM}}{\mathrm{r}^3} \mathbf{r} \tag{4}$$

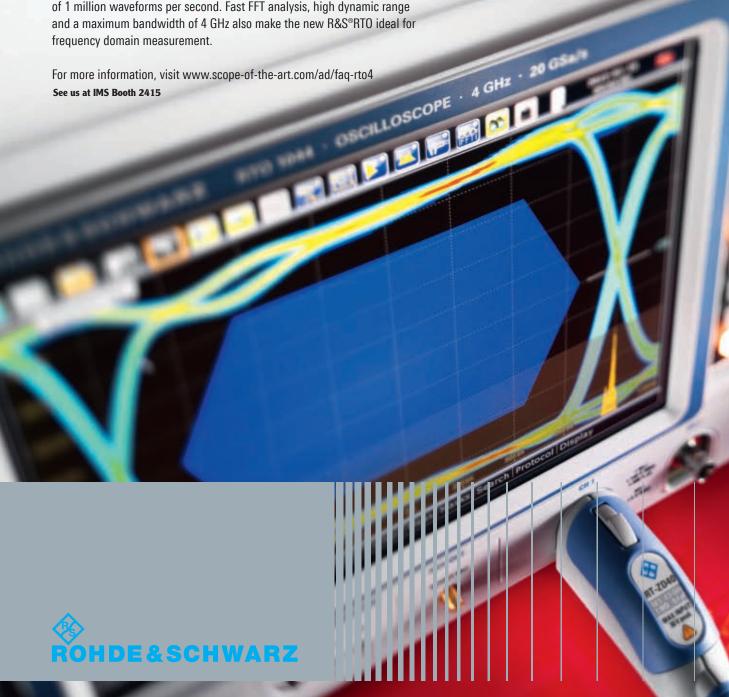
where  $d^2/dt^2$  is the second derivative operator. The solution to Equation 4 can be shown as an ellipse with its focal point located at the center of gravity of the Earth (see **Figure 6**). The

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true anomaly v represents the angle of the satellite in its orbit referenced to the perigee, the orbital point at the shortest distance to the Earth. The semi-major axis of the orbit a and the eccentricity e define the shape of the elliptical orbit and are determined by the location of and the direction in which the satellite is released from its space shuttle.

However, Equation 3 does not describe the motion of the satellite precisely, since ambiguities are caused by the solar and lunar gravitational forces and by the fact that the Earth is not perfectly spherical. This is the reason why GPS and Galileo control stations upload an up-to-date version of the satellite's Keplerian orbit parameters, e.g., a and e, usually every two hours.

After locating the satellite in its orbit, the argument of the perigee w, the longitude of the ascending node  $\Omega$  and the inclination of the orbit i are used to transform the position of the satellite to ECI using a set of rotations as shown in Figure 6. These parameters are transmitted by GPS and Galileo satellites as part of the ephemeris message.

GLONASS satellites, on the other hand, do not transmit any Keplerian parameters in the ephemeris of the navigation message. They simply transmit the location and the velocity of the satellite at a specific epoch in ECEF.

Rotating the differential Equation 4 from ECI to ECEF and updating it to take into account the spherical harmonics and the gravitational forces of the sun and the moon would allow the UE to estimate the position of the satellite in a time span of 30 minutes around the reference epoch. Fourthorder Runge-Kutta numerical methods are usually used by GLONASS receivers to determine the position of the satellite in a span of 30 minutes based on the motion differential equation and the location and velocity of the satellite in ECEF at the reference epoch. The solar/lunar gravitational accelerations in ECEF are also transmitted as part of the ephemeris of GLONASS satellites.

#### **APPLICATIONS**

Different types of GNSS receivers are used, depending on the precision required by the specific application. To understand these applications, it is important first to understand the generic functionality of the different hardware and software modules of a GNSS receiver. The three basic functionalities of a GNSS receiver are described below.

**Acquisition:** The receiver uses open loop circuits to search for the Doppler frequency and the approximate code phase for every visible satellite if enough acquisition channels are available in the device. The code phase search window for GPS is 1023 chips, for GLONASS 511 chips and for Galileo 4092 chips. These are the lengths of the corresponding spreading code of the respective GNSS. The search resolution is usually ½-chip, which maps to around 150 m in GPS, since the chip rate of the coarse acquisition (CA) civilian signal is 1.023 MHz.

The search window for the Doppler usually has a resolution of 50 Hz. Signals are acquired on a per-channel basis, and the up to ½-chip phase-ambiguous signal is passed to the code and carrier tracking loops to achieve perfect signal locking, thereby removing code-phase and frequency ambiguities.

Tracking: The code phase acquired from an acquisition channel has a maximum error of ½-chip (150 m in GPS). The code phase is tracked in a delay locked loop (DLL), which utilizes the special correlation properties of GNSS signals to track and lock the code phase. Locking the carrier phase usually happens in a phase locked loop (PLL). The two tracking circuits are interconnected, since the DLL requires that the PLL eliminate the Doppler shift, while the PLL requires that the DLL provide perfect correlation. Like acquisition, signals are also tracked on a per-channel basis. It would not be possible to track a signal without an acquisition stage that initializes the DLL and PLL, thereby allowing them to converge when tracking the GNSS signal of a specific satellite.

**Navigation:** The navigation algorithm makes use of all the CDMA code-phase and carrier-phase readings (depending on the application) to calculate the position of UE.

#### **STANDARD GNSS**

Standard GNSS receivers usually operate on one frequency band, the

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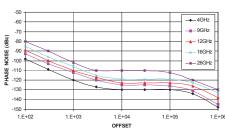
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#### **Technical Feature**

L1/E1 band. GLONASS enhances GPS receivers by increasing the probability to find at least four satellites at a LOS. The precision of standard GNSS receivers is around 10 m.

#### **A-GNSS**

The calculation of a satellite position requires decoding the navigation message. It takes 30 s in GPS to decode one frame containing an ephemeris set, and the receiver cannot get a position fix before decoding the first three subframes (18 s) of a GPS page. As a result, it takes a long time to get a location fix when booting a GNSS receiver. Using A-GNSS, a mobile communications downlink such as CDMA2000 transmits the ephemeris navigation information to the UE, thereby minimizing the time needed by the UE to get a fix to around 1 s.

Additionally, in the UE-assisted mode of A-GNSS, the mobile phone works as a sensor and thus only acquires and tracks code and carrier phases. An assisted server is responsible for locating the UE on the basis of the reported tracking observations from the UE to a base station (BS). The BS, e.g. LTE BS, transmits some acquisition assistant data to the UE prior to the measurement. This data is used by the UE to reduce its code and carrier phase search windows, thereby minimizing the acquisition effort and consequently accelerating the acquisition process of the GNSS sensor.

The acquisition assistant data is simply the acquired code phase and carrier phase or frequency read from a GNSS receiver located at the BS tower. The UE initializes its acquisition code and frequency search windows around the values transmitted by the BS and in this way reduces the size of the acquisition search windows depending on the maximum BS coverage radius.

#### **DIFFERENTIAL GNSS**

As expressed in the generic channel Equation 3, two of the most significant factors affecting the accuracy of determining the position of a satellite are the ionosphere and satellite clock correction ambiguities. The vector (baseline) from a static reference point – which is at a close proximity to the user – to the UE can be determined by simply processing the tracking readings or the ionosphere delay

as well as the satellite clock error of the static reference point at the UE. This makes it possible to eliminate the similar ambiguities in the ionosphere and satellite clock and thus improve the performance of GNSS to 1 m. The transmitted correction data is called differential data. GNSS performance can increase even more if carrier phase readings are additionally used.

Differential corrections are usually transmitted using regional navigation satellite systems, which are also called satellite-based augmentation systems (SBAS). The best known SBAS is the American WAAS providing D-GPS service to North America.

#### **MULTIPLE FREQUENCY GNSS**

Satellites sometimes transmit the same signal on different bands, e.g., GPS on L1 and L2. By combining tracking readings from L1 and L2, it is possible to remove the ionosphere ambiguities. This is because the ionosphere deflection from the LOS is inversely proportional to the square of the carrier frequency. As a result, GNSS performance can be improved to the range of 5 m.

#### CONCLUSION

Although many advanced applications such as multiple frequency GNSS and differential GNSS can improve the performance of GNSS receivers significantly, the commercial solutions are still heavily limited to standard GNSS and A-GNSS because they are easy to implement. In the future, the market trend will continue to move toward combining GNSS signals on common bands such as L1/E1 to increase satellite availability in urban areas.

#### Reference

 E. Kaplan and C. Hegarty, Understanding GPS: Principles and Applications, Artech House, 2006.



Rachid El Assir received his bachelor's degree in electrical engineering from the American University of Beirut in 2003 and his master's of science degree in communications engineering from Munich Institute of Technology in 2005. Since then he has been working on the baseband development of Rohde & Schwarz state of

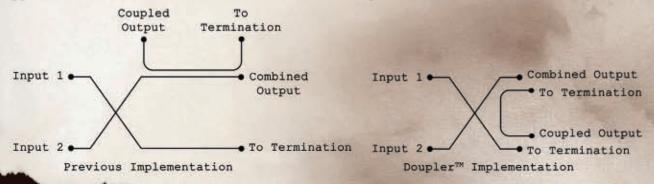
the art signal generators. El Assir currently leads the development of the global navigation satellite systems (GNSS) program on vector signal generators.

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DDDP20F	2500 - 2700 MHz	Doherty Combiner	20-dB Directional	May 2012	
DDDL20F	1805 - 1880 MHz	Doherty Combiner	20-dB Directional	May 2012	
DDDV30F	700 - 800 MHz	Doherty Combiner	30-dB Directional	May 2012	
DHDD30F	925 - 960 MHz	3-dB Hybrid	30-dB Directional	June 2012	
DHDT30F	869 - 894 MHz	3-dB Hybrid	30-dB Directional	June 2012	
DHDV30F	700 - 800 MHz	3-dB Hybrid	30-dB Directional	June 2012	



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## Non-Uniform Defected Microstrip Structure Lowpass Filter

A defected microstrip structure (DMS) has properties similar to a defected ground structure (DGS), but without any leakage through the ground plane. In this article, new lowpass filters with ultra-wide stopband, using non-uniform DMS that is beneficial to higher order harmonic suppression, are presented. A comparison is made to lowpass filters using standard 50  $\Omega$  microstrip lines and stepped-impedance microstrip lines. The proposed lowpass filters have the advantages of good frequency selectivity, ultra-wide stopband and simple circuit topology and it shows that the proposed filter, with stepped impedance microstrip line, has better out of band suppression and enhanced return losses than that with a uniform microstrip line and, simultaneously, the DMS units are smaller, which decrease the circuit size. The validity of the design is demonstrated by experiment.

urrently, the defected ground structure (DGS)<sup>1-4</sup> has been widely employed for RF circuit design and improving RF components performance. DGS increases the effective capacitance and inductance of a microstrip line. It is more efficient for harmonic suppression, especially when using periodical DGSs,<sup>4</sup> which results in a greatly improved stopband, because the EM field is highly concentrated under the microstrip line (ML). However, DGS introduces wave leakage through the ground plane, which brings difficulties with encapsulation.

Compared with DGS circuit, the defected microstrip structure (DMS)<sup>5-7</sup> has no enclosure problems, because there is no leakage through the ground plane. DMS is easier to integrate with other microwave circuits and has an effectively reduced circuit size compared with DGS. Simultaneously, DMS exhibits the

properties of slow-wave, rejecting microwaves at certain frequencies and has an increasing electrical length for certain circuits, which are similar to DGS, but without any manipulation of the ground plane. The defection in the microstrip line creates resonance characteristics in the frequency response.

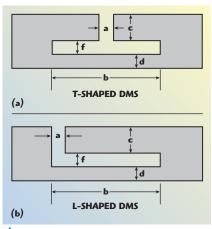
Lowpass filters reject the higher harmonics and spurious responses of circuits, which plays a very important role in RF circuits and systems. The conventional implementation of a lowpass filter (LPF) involves the use of open stubs or stepped impedance microstrip lines. However,

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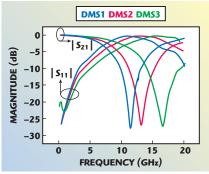


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▲ Fig. 1 Defected microstrip structures.



ightharpoonup Fig. 2 Simulated S-parameter of a 50  $\Omega$  microstrip line with a T shaped DMS unit.

### TABLE I STOP BAND CHARACTERISTICS OF T-SHAPED DMS IN A 50 $\Omega$ MICROSTRIP LINE ( $\mathcal{E}_z$ =2.2, H=0.8 mm)

	DMS1	DMS2	DMS3	
DMS Dimension	a=f=0.4, b=8	a=f=0.4, b=6	a=f=0.4, b=4	
(mm)	d=0.93	d=0.93	d=0.93	
Cut-off Frequency (GHz)	6.83	8.25	10.4	
Attenuation Pole (GHz)	11.2	13.1	16.3	

these structures have a gradual cut-off response. The filter rejection characteristic can only be improved by increasing the number of sections, and this method increases the passband insertion loss and the filter's physical size. In the past few years, some new methods, such as complementary split ring resonators (CSRR),<sup>8</sup> and DGS, especially the periodical DGSs,<sup>4</sup> have been applied to LPF design.

In this article, a new technique for developing DMS assisted lowpass filters with ultra-wideband is presented. The conductor plane of a standard 50  $\Omega$  transmission line and a steppedimpedance transmission line are per-

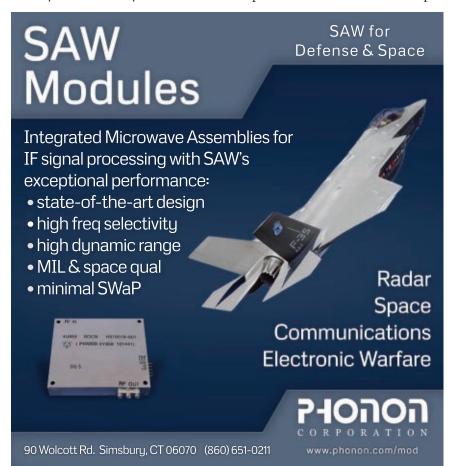
turbed by non-uniform DMS to generate an ultra-wide rejection band that is beneficial to higher order harmonics suppression. New lowpass filters, with good performances of transmission zero and ultra-wide stopband, are designed and a kind of low-

pass filter with DMS cells reduction is fabricated and measured. The experimental results demonstrate the validity of the new design.

#### **DEFECTED MICROSTRIP STRUCTURE**

A conventional DMS consists of a horizontal rectangular slot and a vertical rectangular slot in the middle of a conductor strip, as shown in *Figure* 1. The figure also shows an L-shaped DMS, which is also called a spurline. Similar to the DGS, DMS increases the electrical length of the microstrip line and disturbs its current distribution. As a result, the effective capacitance and inductance of the microstrip line increase. Accordingly, the DMS has slow-wave and stopband characteristics, as the simulation shown in Figure 2 demonstrates, and the dimensions as well as the performance of the DMS are shown in Table 1. It shows that the cut-off frequency of the DMS increases, as the dimension b decreases, so new lowpass filters with ultra-wide stopband can be designed by using these characteristics, because non-uniform DMSs extend the stopband greatly. Here, the simulated results are obtained by using a 50  $\Omega$  microstrip line with a substrate relative permittivity of 2.2 and a thickness of 0.8 mm. The DMS may have more obvious stopband performance by using a substrate with higher permittivity. The electrical performances of stopband for DMS can be simulated by a parallel LC resonant circuit,9 and the equivalent circuit of a DMS matches the response of the 1st Butterworth lowpass prototype, as *Figure* 3 shows. Where:

$$\begin{split} \mathbf{C} &= \frac{\omega_c}{Z_0 g_1} \cdot \frac{1}{\omega_0^2 - \omega_c^2}, \\ \mathbf{L} &= \frac{1}{4\pi^2 f_0^2 C} \end{split} \tag{1}$$



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Here,  $\omega_0$  and  $\omega_c$  denote the resonant frequency and cut-off frequency of the parallel LC resonator, respectively,  $Z_0$  is the characteristic impedance, and  $g_1$  is the normalized parameter of the first Butterworth lowpass prototype.

Calculated variation curves of the external quality factor  $Q_e$ , versus DMS parameters a, c and f are shown in **Figures 4** to **6**, respectively. It

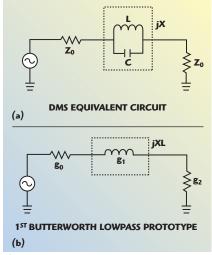


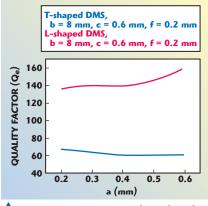
Fig. 3 Equivalent circuit of the DMS and Butterworth lowpass prototype.

shows that for a T-shaped DMS,  $Q_e$  has no obvious variation with parameters a increasing, while  $Q_e$  increases greatly with parameter a increasing. For L-shaped DMS,  $Q_e$  increases with parameter a increasing, while it decreases with parameter a increasing. Both have adequate Q values.

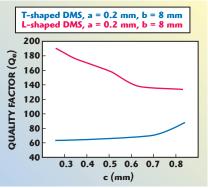
#### NON-UNIFORM DMS LOWPASS FILTERS

#### Lowpass filter with L-shaped DMS

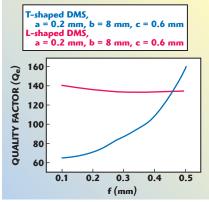
In order to demonstrate a lowpass filter with ultra-wide stopband imple-



ightharpoonup Fig. 4  $Q_e$  vs. parameter a for T-shaped and L-shaped DMS.



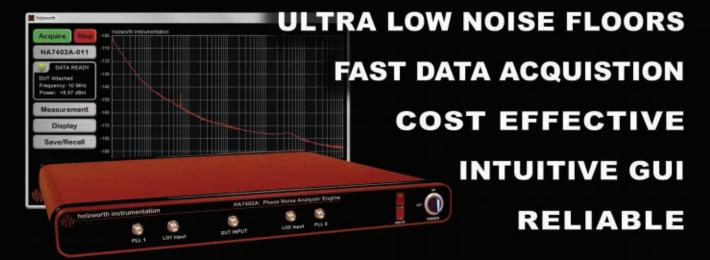
ightharpoonup Fig. 5  $Q_e$  vs. parameter c for T-shaped and L-shaped DMS.



ightharpoonup Fig. 6  $Q_e$  vs. parameter f for T-shaped and L-shaped DMS.

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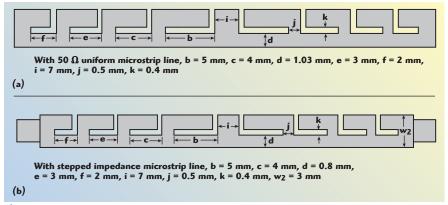
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▲ Fig. 7 L-shaped DMS lowpass filters.

mentation, L-shaped and T-shaped DMS lowpass filters with non-uniform cells are proposed and are designed on Duroid substrates with a relative permittivity of 2.2 and a thickness of 0.8 mm. All the filters are symmetrical structures. The L-shaped DMS lowpass filters with 50  $\Omega$  microstrip line (ML) and stepped impedance microstrip line are shown in *Figure 7(a)* and (b), respectively, and the equivalent circuit model of the stepped impedance ML is shown in *Figure 8*, where  $Z_{01}$  and  $Z_{02}$  can be calculated as 50  $\Omega$  and 43.73  $\Omega$ , respectively. *Fig-*

wre 9 shows the simulated frequency responses of the lowpass filter. It can be seen that with a  $50~\Omega$  uniform ML, the filter has a cut-off frequency of 7.3 GHz, while the filter has a lowered cut-off frequency of 6.12 GHz with the stepped impedance ML. Both have good frequency selectivity and ultra-wide stopband of more than 12.7 GHz, which is 1.6 times the cut-off frequency. Calculated variation curves of the cut-off frequency versus the filter parameter d are shown in **Figure 10**. It shows that the cut-off frequency increases with d increasing

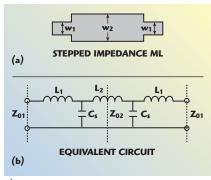


Fig. 8 Stepped impedance ML and equivalent circuit.

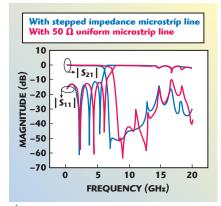
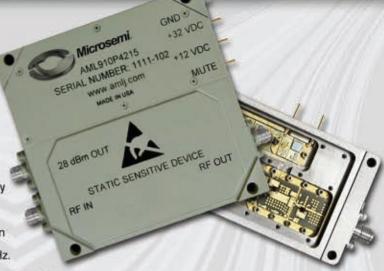


Fig. 9 Simulated frequency responses of the lowpass filter with eight L-shaped DMS cells.





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AML056P4014	0.5 - 6.0	40	37	38	6	28V, 1.0A	20%	EAR99
AML056P4511	0.5 - 6.0	45	39	40	10	28V, 1.3A	25%	EAR99
AML056P4512	0.5 - 6.0	45	43	44	25	40V, 2.7A	23%	EAR99
AML13P5013	1.0 - 3.0	50	46	47	50	28V, 4.8A	25%	EAR99
AML26P4011	2.0 - 6.0	40	40	41	12	28V, 1.5A	30%	EAR99
AML26P4012	2.0 - 6.0	45	43	44	25	28V, 3.0A	30%	EAR99
AML26P4013	2.0 - 6.0	50	46	47	50	28V, 6.0A	30%	EAR99
AML59P4512	5.5 - 9.0	45	45	46	40	28V, 4.0A	35%	3A001.b.4.b
AML59P4513	5.5 - 9.0	45	48	49	80	28V, 8.0A	35%	3A001.b.4.b
AML910P4213	9.9 - 10.7	43	37	38	6	32V, 0.5A	30%	EAR99
AML910P4214	9.9 - 10.7	43	39	40	10	32V, 0.8A	30%	EAR99
AML910P4215	9.9 - 10.7	46	41.5	42	15	32V, 1.3A	30%	EAR99
AML910P4216	9.9 - 10.7	46	42	43	20	32V, 1.3A	30%	3A001.b.4.b
AML811P5011	7.8 - 11.0	45	43	44	25	28V, 2.8A	30%	3A001.b.4.b
AML811P5012	7.8 - 11.0	50	46	47	50	28V, 5.5A	30%	3A001.b.4.b
AML811P5013	7.8 - 11.0	50	48	49	80	28V, 11.5A	25%	3A001.b.4.b
AML1416P4511	14.0 - 16.0	45	42	43	20	35V, 3.2A	18%	ITAR
AML1416P4512	14.0 - 16.0	45	45	46	40	35V, 6.2A	18%	ITAR
AML618P4014	6.0 - 18.0	40	39	40	10	32V, 2.8A	12%	ITAR
AML618P4015	6.0 - 18.0	40	42	43	20	32V, 4.9A	12%	ITAR
AML218P4012	2.0 - 18.0	35	37	38	6	32V, 1.5A	13%	ITAR
AML218P4011	2.0 - 18.0	40	39	40	10	32V, 2.8A	12%	ITAR
AML218P4013	2.0 - 18.0	38	42	43	20	32V, 4.9A	12%	ITAR

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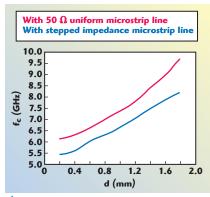
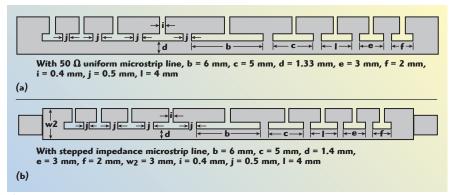


Fig. 10 Variation of the cut-off frequency vs. parameter d.

and the cut-off frequency of the filter with a 50  $\Omega$  ML always has a larger value than that with a stepped impedance ML, when they have the same parameter d.

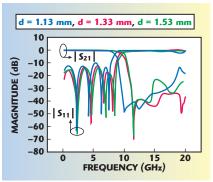
#### **Lowpass filter with T-shaped DMS**

Proposed lowpass filters with ultrawide stopband by using non-uniform T-shaped DMS are shown in *Figure* 11. Their operation principle is the same as that of the L-shaped DMS filter. The simulated frequency responses of the lowpass filter with 50



▲ Fig. 11 T-shaped DMS lowpass filters.

Ω microstrip line by using nine T-shaped DMS non-uniform cells are shown in *Figure 12*. It can be seen that the lowpass filter has transmission zeros, good out of band suppression and an ultra-wide stopband of more than 10 GHz. The filter cut-off frequency decreases with the parameter d decreasing. *Figure 13* shows the simulated frequency responses of the lowpass filter with different DMS cells. It can be seen that the lowpass filter with nine DMS cells and seven DMS cells nearly have the same cut-off frequency of approximately 9.45



A Fig. 12 Simulated frequency responses of the lowpass filter with 50 Ω microstrip line and nine T-shaped DMS cells.



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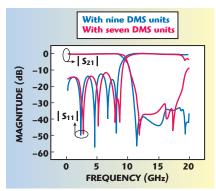


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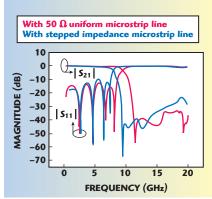


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ightharpoonup Fig. 13 Frequency responses of the lowpass filter with seven and nine DMS cells, using a 50  $\Omega$  microstrip line.

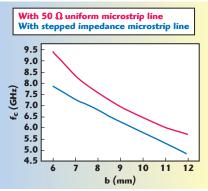
GHz. However, the former has a wider stopband than the later because more non-uniform DMS cells bring a larger reject band range. *Figure 14* shows the frequency responses of the lowpass filter with nine DMS cells, using uniform microstrip line and stepped impedance microstrip line. *Figure 15* shows the variation curves of cutoff frequency versus the filter physical parameter b. It can be seen that the lowpass filter with stepped impedance ML shows a lower cut-off frequency, which correspondingly introduces a



ightharpoonup Fig. 14 Frequency responses of the lowpass filter with nine DMS cells, using 50  $\Omega$ microstrip line and stepped impedance microstrip line.

wider stopband than that with a 50  $\Omega$  uniform ML. It also can be seen that the filter cut-off frequency decreases with the parameter b increasing.

It is known that the stopband is related to the number of DMS cells, and a wider stopband always leads to a larger circuit size. Here, lowpass filters with five T-shaped DMS cells are also designed, in order to reduce the circuit size, as *Figure 16* shows. The simulated frequency responses are shown



▲ Fig. 15 Cut-off frequency vs. parameter b for the lowpass filter with nine DMS cells.

in *Figure 17*. It shows that the filter has an ultra-wide stopband of approximately 2.45 times the cut-off frequency of 5.8 GHz and the stepped impedance ML introduces a better out of band suppression and a better passband return loss than the uniform ML. Variation curves of cut-off frequency versus parameters b and d for the lowpass filter with reduced DMS cells are shown in *Figures 18* and *19*, respectively. They show that the cut-off frequency decreases with b increasing, while it increases with d increasing, and a larger



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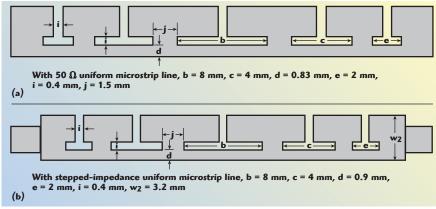


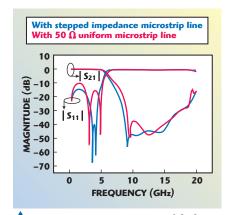
Fig. 16 T-shaped DMS lowpass filter with reduced cells.

d introduces a larger difference on filter cut-off frequency between uniform and stepped impedance MLs.

In order to verify the design, a lowpass filter, as shown in Figure 16(b), was fabricated and measured and the hardware, which has a circuit size of no more than  $40\times3.2$  mm is shown in **Figure 20**. The figure also shows the measured performances, taken with an Agilent E5071C vector network analyzer. The measured results are similar to the simulation. The measured discrepancies are mainly due to the simulation precision and fabrication uncertainty.

#### **CONCLUSION**

New microstrip lowpass filters, with ultra-wide stopband by using periodical non-uniform DMS, are designed and a comparison between lowpass filters with uniform  $50~\Omega$  and stepped-impedance microstrip lines is made. It shows that, with stepped-impedance microstrip line, the filter has enhanced return losses and better out of band suppression. The new



 $\blacktriangle$  Fig. 17 Frequency responses of the lowpass filter with reduced DMS cells, using 50 Ω and step impedance microstrip lines.

design is demonstrated by measurement. Compared with DGS assisted lowpass filter, the DMS lowpass filter has a simpler topology and is easier to fabricate. Most importantly, it has no enclosure problem, because there is no leakage from the ground plane.

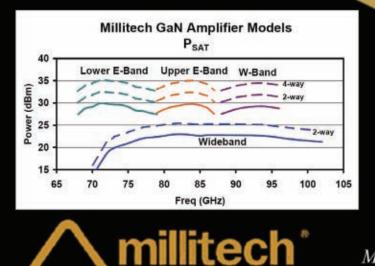
#### **ACKNOWLEDGMENT**

This work was supported in part by the Open Research Fund of China State Key Laboratory of Millimeter Waves (K201107).

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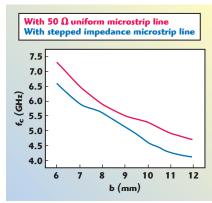
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▲ Fig. 18 Cut-off frequency vs. parameter b for the lowpass filter with reduced DMS cells.

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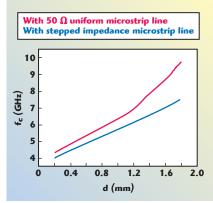


Fig. 19 Cut-off frequency vs. parameter d for the lowpass filter with reduced DMS cells.

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**MEASUREMENT** 

SIMUL ATION

15

▲ Fig. 20 The fabricated filter (a) and its performance (b).

FREQUENCY (GHz)

50

-60

(b)

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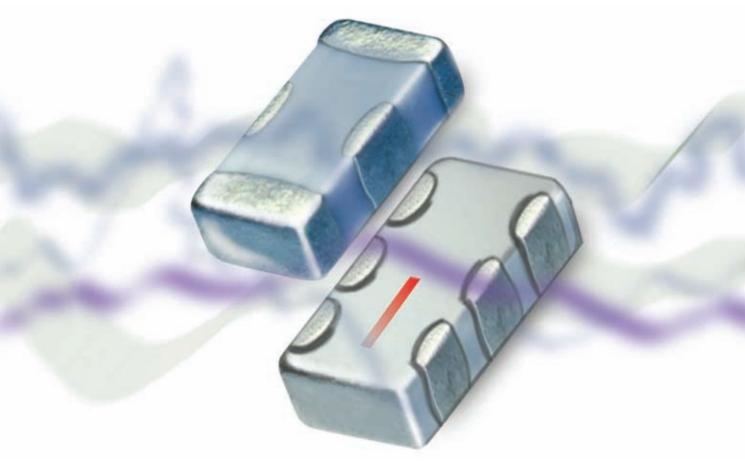
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raditionally, GaAs based technologies capable of providing solutions at E- and W-Band have been limited to three- and four-inch wafer processing techniques with associated higher running costs. These technologies have generally provided excellent performance but with limited acceptance in moderate volume markets due to associated high MMIC component cost. With the emergence of volume markets in these bands, low-cost GaAs based component solutions are required to meet the cost demands of markets such as E-Band point-to-point communication applications (71 to 76 GHz and 81 to 86 GHz), automotive radar (76 to 77 GHz) and radar systems (93 to 95 GHz).

High frequency point-to-point communication bands at E-Band offer the potential for ultra-high capacity links. The large allocated band offers fiber-like Gbps data rates that far exceed the present performance of the lower frequency microwave radio bands. The ease of installation of the links compared with fiber based solutions point toward this being a long-term solution for high data rate communications in many countries. In the automotive market, autonomous cruise control and emergency braking systems have been developed and successfully deployed on top-end models but until now wider usage has been restricted by the high cost of millimeter-wave components. In these markets and the mainly aerospace focused 94 GHz radar markets, the availability of low cost MMIC based components offers the route to wider market expansion.

Therefore, a key enabling technology for the long-term volume uptake will be the availability of cost-effective semiconductors capable of delivering the required performance at E-Band and above. Recently, GaAs foundries have focused on employing many of the processing techniques and equipment used in the high volume applications of mobile terminals to provide low-cost solutions targeted at these higher frequencies. This has resulted in the release of high performance GaAs based technologies capable of delivering significant gain and power up to W-Band. High performance GaAs based solutions on six-inch wafer technology have the potential to yield low-cost products in the frequency range from 60 to 100 GHz. The enhanced performance of GaAs based solutions, particularly in terms of power and linearity, together with lower development costs makes this the technology of choice on which to develop key functions for volume E- and W-Band applications.

This article describes the design and manufacture of a set of E- and W-Band MMIC power amplifiers based on six-inch 0.1  $\mu$ m GaAs technology. An overview of the circuit architectures for 22 dBm output power amplifier designs is provided. Measured results of manufactured MMICs show good agreement with simulated results thus demonstrating GaAs MMIC capability to meet the requirements for high performance, low cost E- and W-Band applications.

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TABLE I  E- AND W-BAND HPA MMIC DESIGN SPECIFICATIONS							
	E-Band (81 to 86 GHz)			W-Band (93 to 95 GHz)			
	LPA	MPA	HPA	LPA	MPA	HPA	
Gain (dB)	20	12	10	20	12	10	
Output Power (dBm)	17	19.5	22	17	19.5	22	
Linearity (dBm)	>23	>25	>27				

#### E- AND W-BAND MMIC AMPLIFIER DESIGN

The aim of the design process was to realize amplifiers at a range of power levels in the commercial E-Band communication band at 81 to 86 GHz and in the radar band in the 93 to 95 GHz range. Successful demonstration of frequency and power in these bands can be easily translated to the less challenging design at the lower frequency applications in the 60 to 76 GHz range.

The design philosophy was based on realizing low power amplifiers (LPA), medium power amplifiers (MPA) and high power amplifiers (HPA) in each of the bands. The target specification for each of the amplifiers is shown in **Table 1**. The LPA can be configured as a local oscillator (LOA), low-noise amplifier (LNA) or as a driver amplifier in the transmit or receive chain. The aim of the HPA

specification is to meet the requirements for the output stage of the transmit section for an E-Band radio or as a single MMIC in a multi-MMIC combined HPA for radar applications. In the three design cases, similar circuit features, design approaches and simulation techniques were employed.

The set of E- and W-Band amplifiers were designed on WIN Semiconductor's PP10 technology which is a 0.1 μm GaAs PHEMT process manufactured on 150 mm wafers. PP10 has an  $F_t$  > 135 GHz and  $F_{max}$  > 185 GHz and is capable of 4 V operation. 1 Measured data of the PP10 PHEMT devices was used to ascertain the optimum periphery in terms of power and gain to meet the requirements for each of the amplifiers. Small-signal S-parameter data was supplied by the foundry for a range of different devices sizes (unit gate width and number of fingers). Also, loadpull data was available for a  $2\times50~\mu m$  sized device measured at 30 GHz.<sup>2</sup> A G<sub>MAX</sub> of greater than 10 dB is available for  $2\times25$  and  $2\times50$  µm sized devices. In circuit, this level of gain will not be achieved due to interstage and output network losses, matching for optimum power rather than gain and the influence of any lossy stabilization networks. Published loadpull data indicates that a saturated power density of approximately 0.8 W/mm from a 4 V supply can be achieved. Higher frequency power density data was not available during the design process which offered a level of risk in extrapolating the power density to E- and W-Band. However, the level of gain and low frequency power density indicated that the technology was capable of



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realizing good amplifier performance in the E- and W-Band.

The LPA was realized as a three-stage design based on  $2\times50~\mu m$  cells for each stage. Although the  $2\times25~\mu m$  cell offered the potential for higher gain, the  $2\times50~\mu m$  cell offered adequate gain coupled with the potential for meeting the power requirements. The four fingered cell approach  $(4\times25~\mu m)$  indicated a lower available gain, which may be due to

phasing issues across the device due to the narrow input and output feeds for available devices. A common 50  $\Omega$  matched structure was used for each stage. This allowed for the potential to easily convert to more stages, or to employ the common cell in multifunction MMICs with other circuit types. The matching networks at the input and output of the  $2\times50~\mu m$  device consisted of a short transmission line and an open circuit stub. Bias was

applied to the gate and drain of the PHEMT cells through a bias network consisting of a resonant radial stub and a one quarter wavelength high impedance line. On the power supply side of the radial stub, further lossy decoupling networks were employed to provide a non-reactive termination at low frequencies to ensure oscillation free operation. MIM capacitors were employed to provide DC blocks in the input, interstage and output networks. Further stabilization networks were employed in the input and interstage networks through a parallel R-C network. The intention of this structure was to reduce the lower frequency gain while having a negligible impact on the in-band performance.

A critical aspect of the design is to understand sensitivity of the circuit and to find the best solution for simulation. Previous experience with HPA and amplifier design at lower frequencies pointed toward an approach based on intensive EM simulation of all passive elements; AWR Axiem was employed for the EM simulations. The procedure involves EM simulating entire matching structures and understanding the influence of the active devices on the passive circuit performance. Some level of discrepancy between schematic based and initial EM simulated behavior was present. The circuit was re-tuned until the EM based modeled performance met the

electrical requirements. A similar process was employed for the design of the MPAs. The MPA consisted of two stages of gain. In this case, the output periphery was realized as  $2\times2\hat{\times}50$  µm cells. The two cells were directly combined together in a corporate matched configuration. Although an in-circuit gain of greater than 6 dB is present, the same size driver periphery as the output periphery was employed. This was to ensure that the driver stage had a negligible impact on the power saturation and linearity of the MMIC over the full temperature range and expected process spread. The downside of employing the larger driver is an increase in the DC power consumption and thus a reduction in the total efficiency. Similar circuit features were employed in the MPA as the LPA, in order to apply bias, stabilize the circuit and extract maximum power. Further stability analysis was employed in the MPA to





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ensure the absence of 'odd-mode' and loop oscillation.<sup>3,4</sup>

The HPA designs employed  $4\times2\times50~\mu m$  cells in the output stage in order to realize greater than 22 dBm of output power. A two stage design was used in order to meet the gain requirements as presented in Table 1. The HPAs were based on two channels of the MPAs which are combined in a corporate approach. This offers a relatively simple and modular approach to increasing the periphery

and thus the output power. Further EM simulations were employed in order to ensure that coupling between the two channels was minimal. The symmetry of the HPA is critical, in order to ensure that power is combined in phase.

#### **MEASUREMENTS**

All amplifiers were mounted on a copper tungsten carrier with thermal epoxy. In order to obtain oscillation free operation, external decoupling

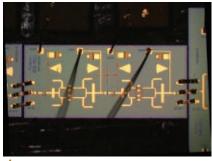


Fig. 1 Assembled carrier for E-Band HPA device measurements.

networks must be applied to the gates and drains of each stage. In a production test environment this can be readily achieved with a custom probe card with integrated decoupling. In this characterization 100 pF single layer ceramic capacitors were bonded to each gate. Further decoupling was applied through bonding universal DC boards consisting of higher value 0402 capacitors onto each gate and drain. Bias was applied to the amplifiers through connecting DC probes to the DC boards. The amplifiers were all directly RF probed and characterized from 75 to 110 GHz. Figure 1 shows a typical configuration for characterization showing a photograph of the E-Band MMIC line-up with associated decoupling networks.

Small-signal measurements were carried out at the Technical University of Graz in Austria. The set uses a ZVA-67 with frequency extensions up to 110 GHz. A set of large-signal measurements were carried out at Filtronic Broadband Ltd. in order to ascertain the power saturation and linearity characteristics of the 81 to 86 GHz amplifier sets. In order to provide sufficient source power, the LPA and MPAs were used as driver devices to provide high gain chains for the HPAs.

Figure 2a shows the small-signal measured performance of the 81 to 86 GHz LPA. Approximately 20 to 22 dB of gain is achieved across the band with an output return loss of better than 11 dB and an input return loss of greater than 8 dB. Figure 2b shows the measured performance of the W-Band LPA that is designed to operate in the 93 to 95 GHz band. Approximately 18 dB of gain is achieved with an input return loss of better than 10 dB and an output return loss of greater than 10 dB. Levels of gain and return losses are close to the sim-





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ulated performance for both MMICs. *Figure 3a* shows a measured power sweep for the E-Band LPA at 83 GHz. The saturated power is greater than 17 dBm at the center of the band. This indicates an 'in-circuit' power density of approximately 0.6 W/mm that is similar to the expected performance based on the lower frequency extrapolated loadpull data. The best P1dB was achieved when biasing the LPA in a Class AB mode that is at an op-

erating condition away from the peak gain bias point. *Figure 3b* shows the measured OIP3 as a function of swept power. The best performance was achieved with a bias point of  $V_{DS}$ =4 V and  $V_{GS}$ =-0.5 V for each stage. A peak output OIP3 of 24 dBm was achieved at a total output power of +10 dBm.

Figure 4a shows the small-signal measured performance of the 81 to 86 GHz MPA. The design is based on a two-stage configuration and exhibits a

measured small-signal gain of 12 dB with return losses of better than 10 dB across the band. *Figure 4b* shows the measured performance of the corresponding W-Band MPA with 11 dB of small-signal gain and return losses

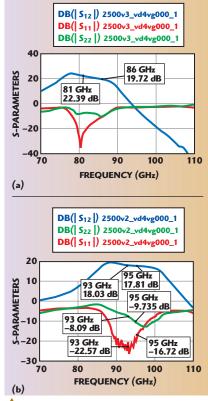
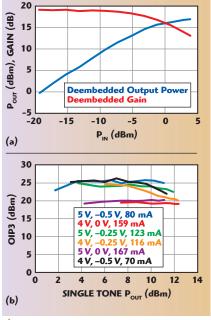


Fig. 2 Measured small-signal performance of E-Band LPA (a) and W-Band LPA (b).



▲ Fig. 3 Measured power sweep for E-Band LPA at 83 GHz (a) and OIP3 at 84 GHz (b).

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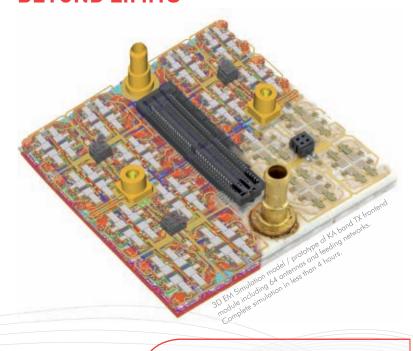
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of greater than 10 dB across the required frequency band. The E-Band MPA was measured under large-signal conditions and a saturated power of greater than 19.5 dBm was achieved. This is typically in-line with the power density measured for the E-Band LPA previously.

Figure 5a shows the measured small-signal performance of the E-Band HPA. A measured gain of greater than 10 dB and with return losses of greater than 10 dB was achieved.

*Figure 5b* shows the measured smallsignal performance of the W-Band HPA; greater than 10 dB of gain was achieved with good return losses across the required frequency range. As mentioned previously, in order to measure the power and linearity characteristics of the HPA, the LPA and MPA were employed as driver stages. The devices were connected together through low-inductance chip to chip tape bonds. Figure 6a shows the power sweep for this configuration,

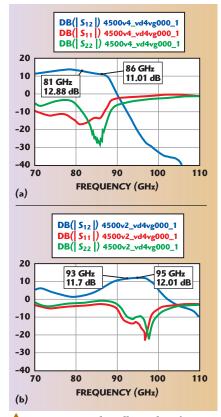


Fig. 4 Measured small-signal performance of E-Band MPA (a) and W-Band MPA

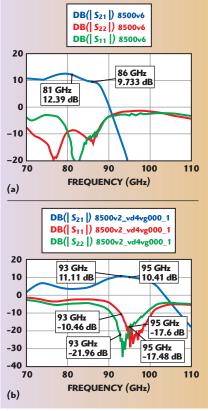


Fig. 5 Measured small-signal performance of E-Band HPA (a) and W-Band HPA



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biased in a Class AB mode for the center of the frequency band. A saturated power of greater than 22 dBm is achieved in the center of the band, with a P1dB of 21 dBm. This level of saturated power density is similar to that achieved for the LPA and MPA. A slight degradation of the in-circuit power density would be expected due to the extra output combining losses. The OIP3 of the line-up of gain stages is shown in *Figure 6b*. The measured OIP3 is between 29 to 30 dB for total

powers up to  $+17~\mathrm{dBm}$ . As the output power reaches close to the onset of power saturation, a roll-off in OIP3 is evident. The total gain of the amplifier chain in this configuration is approximately 30 dB.

### **CONCLUSION**

E- and W-Band power amplifier MMICs have been designed on sixinch 0.1  $\mu m$  GaAs technology. Measured results of the manufactured MMICs demonstrated good agree-



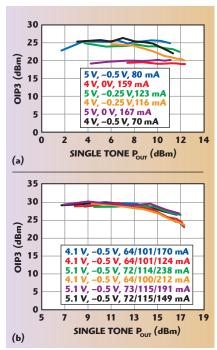


Fig. 6 Measured power sweep for E-Band HPA at 83 GHz (a) and OIP3 at 82 GHz (b)

ment with simulated results: low power amplifier devices achieved good levels of gain in excess of 20 dB for both E- and W-Band devices. The HPA devices achieved saturated output powers in excess of 22 dBm; tuning of the matching environment will provide further optimized performance. Furthermore, the circuit architecture employed can be easily extended to provide higher levels of output powers. The results presented here demonstrate GaAs MMIC capability is available today to meet the next generation requirements of high performance, low cost E- and W-Band applications.

### **ACKNOWLEDGMENTS**

We would like to thank the Technical University of Graz (www.ihf. tugraz.at) and Filtronic Broadband (www.filtronic.co.uk) for assistance with measurements.

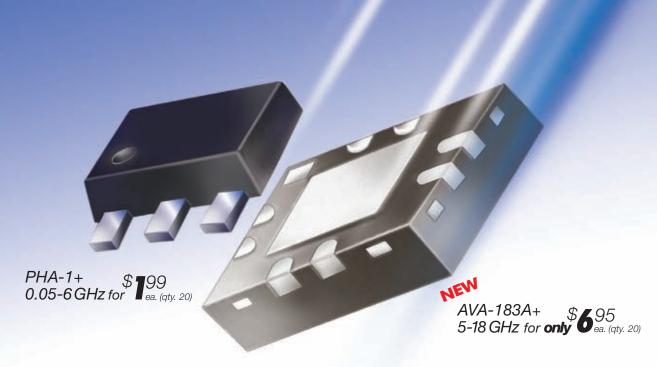
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# Compact UHF Fifth Order Bandpass Filter Using Cascaded Triplet CRLH-ZORs

A bandpass filter is proposed, miniaturized by composite right- and left-handed (CRLH) zeroth order resonators (ZOR), which form a cascaded triplet (CT) to have a significantly sharp skirt for high frequency selectivity. A fifth order UHF bandpass case is tested. First, an in-line ZOR bandpass filter is designed, whose total size is almost 20 percent of a parallel-edge coupled filter. Second, multiple transmission zeros (TZ) are created by changing the three innermost ZORs of the in-line filter to a CT. As a result, with an insertion loss better than 1.5 dB and a return loss better than 15 dB, the size-reduction effect and the skirt of the proposed filter are 24 times smaller than a lower-order parallel-edge coupled filter and as sharp as a  $10^{th}$  order Chebyshev filter. The simulation and measurement validate the proposed design method and the CRLH ZOR properties are proven by the no-phase variation electric field and dispersion diagram.

as the social and business network is expanded and globalized, the demands and users of mobile communications increase by the day. Mobile communication uses several channels, which should be isolated from the adjacent channels. In wireless communication systems, high selectivity of a channel is made possible by bandpass filters with sharp skirts.

Quendo et al introduced a combline filter with a small occupied size and sharp frequency selectivity. Vince also brought the design of a combline filter to have channel selectivity and reduced size. But the performance of the combline filters was not completely optimized. Their design can be improved with TZs near

the passband edge, like the gapped and coupled loop filter Park et al showed.<sup>3</sup> However, their filter does not have a steep skirt and has a narrow matched band, due to the fact that its transfer function has a low order and TZs are not in the effective vicinity of the passband. Tang used multiple resonators to increase the order of the bandpass filter and loaded the structure with capacitive coupling elements to determine the locations of TZs and obtained a steeper skirt in the form of a stacked paralleledge coupled filter.<sup>4</sup> In line with increasing the

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order of a filter, multiple resonators or modes are adopted and cascaded in groups, with cross-coupling paths (CCP) embedded to maximize the frequency selectivity and minimize the overall size, in the name of cascaded quadruplet (CQ), cascaded triplet (CT), etc.<sup>5-8</sup> In most cases, CT and CQ methods go with waveguide cavity filter and multiplexer development and their synthesis scheme is described, accompanying the frequency responses with extremely sharp skirts due to high quality factors, TZs and filter orders.<sup>5-7</sup>

A CT filter can be made with microstrip lines, which has a center frequency of 1.05 GHz.8 The CCP of the CT results in a TZ and steepens its skirt. All the aforementioned filters have restrictions in significant size-reduction, since their resonators are multiples of half-wavelength, determined by the frequency of interest. Particularly, waveguides are not proper for the commercial communication bands such as the UHF, PCS, DCS and ISM. To overcome the limitations of the conventional design methodologies, metamaterials can help RF component designers. 9-12 Since the CRLH lines and ZOR were suggested by Caloz et al,<sup>9</sup> the no-phase variation phenomenon as  $\beta = 0$  and the nonlinear dispersion relation have been used to design sub-wavelength resonators and compact filters. 10,12 The CRLH ZOR filters and the ENZ and MNZ filter<sup>11</sup> show improvement in reducing the size, but have relatively low frequency selectivity.

In this article, a compact CRLH ZOR bandpass filter is designed to have a remarkably enhanced frequency selectivity, working in the UHF band. First, a fifth order in-line ZOR bandpass filter is designed as the initial step. In this step, it is shown that the overall size of the initial filter is approximately 20 percent of that of a parallel edge coupled filter and the metamaterial characteristics are verified by the no-phase varying electric field and the dispersion diagram of the ZOR through simulations. Second, to have a steep skirt, a CT is formed by providing the phase-difference type of cross-coupling in the three innermost ZORs of the inline ZOR filter, which creates TZs in the proximity of the

passband edges. A further size-reduction due to the CT formation is addressed, with the total size of the proposed filter 24 times smaller than even a fourth order parallel edge coupled filter, along with the high frequency selectivity

SPECIFICATIONS OF THE BANDPASS FILTER			
Specification			
950 MHz			
350 MHz			
≤ 2 dB			
≤ 15 dB			
≥ 20 dB			

equivalent to the  $10^{\rm th}$  order Chebyshev filter. Besides, the low insertion loss better than 1.5 dB and the low return loss better than 15 dB are obtained with a lossy FR-4 substrate. To examine the validity of the proposed design method, the circuit and 3D EM simulations are carried out and are in good agreement with the measurements of the fabricated prototype of the CT CRLH ZOR bandpass filter.

### DESIGN OF THE IN-LINE CRLH ZOR BANDPASS FILTER

The bandpass filter is designed on the basis of the specifications shown in  $\it Table~1$ . The GSM communications in the UHF band require that  $f_{ue}$ , as the band upper edge, equals  $f_0$  + BW/2. To avoid the unwanted interference from the PCS,  $S_{21}$  should be attenuated to lower than -20 dB at the frequency  $f_{ue}$  + 50 MHz. The sharp skirt will be excluded in this step to design the in-line ZOR bandpass filter, but will be included in the next step. To begin with, the aforementioned specifications, except for the skirt, can be obtained with the following transfer function:

$$S_{21}(s) = \frac{.1789}{s^5 + 1.172s^4 + 1.937s^3 + 1.31s^2 + .7525s + .1789} \quad (1)$$

where s is j $\omega$  and  $\omega$  is the angular frequency.

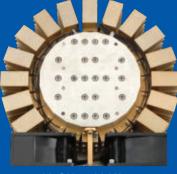
The fifth order equivalent circuit is shown in *Figure 1*. It comprises resonators 1 through 5 and their coupling ele-





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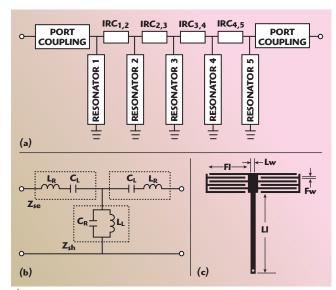
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▲ Fig. 1 Equivalent circuit (a), CRLH equivalent circuit of the CLRH ZOR resonator (b), and its physical shape (c).

ments named  $IRC_{i,j}$ , which means that the inter-resonator coupling is between resonators i and j. Each resonator is made of a shunt inductor and capacitor.  $IRC_{i,j}$  is chosen as a series inductor. In the conventional filter design, the physical structure for the resonators will be half-wavelength open-ended microstrip. But here, the CRLH ZOR for each of the resonators and the ordinary shunt inductor and capacitor in the resonator should be changed to the CRLH configuration, following the formula given by Jang and Kahng,  $^{10}$  with the following equations for the bandedge (or cut-off) frequencies, center frequency and impedance of the CRLH ZOR.

$$\omega_{L} = \frac{1}{\sqrt{L_{L}C_{L}}}, \omega_{R} = \frac{1}{\sqrt{L_{R}C_{R}}}, \omega_{se} = \frac{1}{\sqrt{L_{R}C_{L}}},$$

$$\omega_{sh} = \frac{1}{\sqrt{L_{L}C_{R}}}, \omega_{0} = \sqrt{\omega_{R}\omega_{L}}$$
(2)

$$\begin{split} Z_{\rm L} &= \sqrt{\frac{L_{\rm L}}{C_{\rm L}}}, Z_{\rm R} = \sqrt{\frac{L_{\rm R}}{C_{\rm R}}}, Z_{\rm se} = \frac{1 - \omega^2 L_{\rm R} C_{\rm L}}{j\omega C_{\rm L}}, \\ Z_{\rm sh} &= \frac{j\omega L_{\rm L}}{1 - \omega^2 L_{\rm L} C_{\rm R}} \end{split} \tag{3}$$

where the subscripts R, L, se and sh are the right-handed, left-handed, series and shunt, in that order.

The circuit elements for the CRLH ZORs 1 through 5 are calculated as  $C_L$  = 1.31 pF,  $C_R$  = 0.70 pF,  $L_L$  = 7.37 nH,  $L_R$  = 0.80 nH for ZOR 1 and ZOR 5,  $C_L$  = 1.34 pF,  $C_R$  = 1.40 pF,  $L_L$  = 5.67 nH,  $L_R$  = 0.50 nH for ZOR 2 and ZOR 4 and  $C_L$  = 1.31 pF,  $C_R$  = 0.70 pF,  $L_L$  = 7.43 nH,  $L_R$  = 0.80 nH for ZOR 3. These circuit elements are converted to the initial values of the physical dimensions using the following approximate formulas considering a microstrip on a 50 mil thick substrate of relative dielectric constant 4.4.

$$L_{\rm L} = \frac{Z_{\rm C}}{\omega} \tan \left( \beta_{\rm eff} l \right) \tag{4}$$

$$C_{L} \approx (\varepsilon_{r} + 1)l[(n-3)A_{1} + A_{2}](pF)$$
(5)

$$A_{1} = 4.409 \tanh \left[ 0.55 \left( \frac{h}{w} \right)^{0.45} \right] 10^{6} \left( \frac{pF}{\mu m} \right)$$
 (6)

$$A_2 = 9.92 \tanh \left[ 0.52 \left( \frac{h}{w} \right)^{0.5} \right] 10^6 \left( \frac{pF}{\mu m} \right)$$
 (7)

The physical dimensions are varied from the initial values in the 3D EM simulation and reach the final values, when

they give the center frequency at the desired value (950 MHz). The final physical dimensions are summarized for ZORs 1 and 5 in  $Table\ 2$ . With these values, the  $S_{21}$  and  $S_{11}$  parameters of

TABLE II						
CIRCUIT AND PHYSICAL ELEMENT VALUES IN FIGURE 1						
Variable Value Variable Value						
$C_{\mathrm{L}}$	1.31 pF	$L_{w}$	1.4 mm			
$C_R$	0.70 pF	$L_{\rm e}$	17.4 mm			
$L_{ m L}$	7.37 nH	$F_l$	6.3 mm			
$L_R$	0.80 nH	$F_{\rm w}$	0.1 mm			



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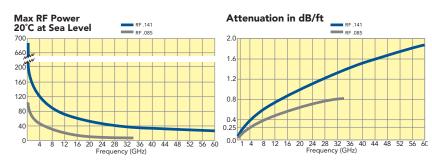
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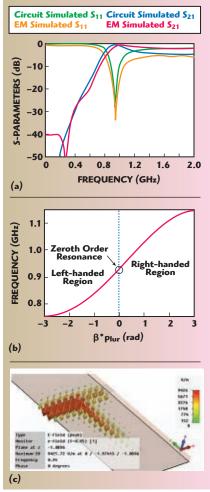
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ZOR, the dispersion diagram, and the metamaterial field distribution are shown in *Figure 2*. The figure reveals



 $\blacktriangle$  Fig. 2  $S_{21}$ ,  $S_{11}$  (a), dispersion diagram (b) and field distribution (c) of the CRLH ZOR.

that the ZOR is appropriately implemented to resonate at  $f_0$  and the circuit simulation agrees well with the 3D EM analysis result of the ZOR, whose size is  $0.05\lambda_g$  (with respect to  $f_0$ ). It is noted that because this is the resonator level, the desired passband will be made in the upcoming level for a complete filter. The dispersion diagram, which has  $\beta$  times the unit-cell length vs. frequency, shows  $\beta=0$  as the ZOR coincides with  $f_0$ . Besides, the right- and

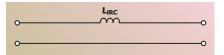


Fig. 3 Equivalent circuit of the inductive coupling between ZORs.

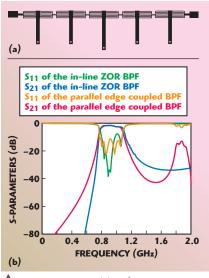


Fig. 4 Geometry (a) and S-parameters (b) of the fifth order in-line CRLH ZOR filter.

left-handed regions occur beyond and below the ZOR as the positive and negative  $\beta,$  respectively. Together with the dispersion diagram, another property of this CRLH metamaterial structure is given as the no-phase variation electric field. All the field vectors of  $\beta$  = 0 have the same direction at the ZOR frequency point.

Until now, the resonators have been addressed. Now, the coupling between neighboring ZORs is added to make a filter with the passband and stopband satisfying the specifications. In a symmetric in-line bandpass filter, the outer and inner inductive lines, named  $L_{IRC}$  in *Figure 3*, of 3.0 and 3.8 nH as the initial numbers for  $IRC_{1,2}$  and  $IRC_{2,3}$ , respectively, are considered and varied in the iterative 3D EM simulations until the bands are made close to and coincident with the specifications.

The inductive line can be realized by the inductance from the distributed transmission line, as shown in the figure, not needing the extra inductance of a lumped element like a chip inductor. So the filters are fully printed throughout this article.

The in-line filter in *Figure 4* has five of the ZORs proposed with the coupling elements to effectively miniaturize the overall size. In detail, the total length of the proposed in-line filter is less than 65 mm, while one resonator of the conventional parallel edge coupled filter is approximately 90 mm long. This means a significant effect in the size reduction brought by the present

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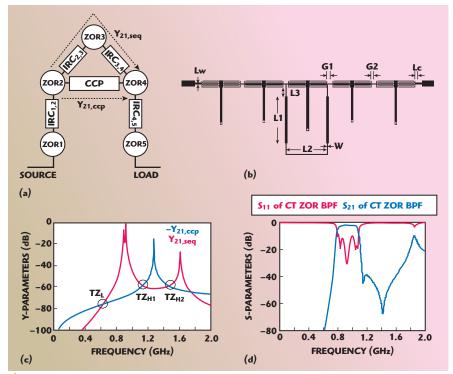
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### **Technical Feature**



lacktriangle Fig. 5 Schematic of the proposed CT ZOR bandpass filter (a), the preliminary shape of the filter (b),  $Y_{2l ext{-}seq}$  and  $-Y_{2l ext{-}ccp}$  (c) and S-parameters (d).

work. In the next section, the size will be further reduced by taking the form of a CT. As another benefit, this in-line ZOR filter provides that the first harmonic at  $1.9 \text{ GHz} (= 2f_0)$  of the parallel edge coupled filter is shifted away and the stopband is widened for the in-line ZOR filter, which the nonlinear dispersion accounts for. With regard to the insertion loss and the return loss, the related specifications are not satisfied with the in-line filter, but this is the first step in the entire design of this article, and this matter will be mitigated in the next step. Also, the smoothly varying skirt  $(S_{21}^{1} \approx -11 \text{ dB at } f_{ue} + 50 \text{ MHz}) \text{ will be}$ totally changed in the upcoming section.

### DESIGN OF THE PROPOSED CT ZOR BANDPASS FILTER

Compliant to the passband, insertion loss and return loss of the specifications, the initial design as the fifth order in-line ZOR filter must be improved for steeper skirts with this configuration. The schematic of *Figure 5* looks similar to that of Figure 1, but it becomes different as the three innermost ZORs (ZOR two, three and four) from the first design step are grouped into a CT, which plays the key-role in generating TZs, by providing the phase difference between the sequential path and cross-coupling path (CCP). The figure also shows the CCP

for the CT. As the preliminary CT ZOR filter, the line parallel coupled to the stubs from the interconnection between the ZORs two and three and another from ZORs three and four is the CCP that couples ZORs two and four. To find the geometric elements of the preliminary CT ZOR filter, the goal is set at the TZs from  $Y_{21,seq}$  +  $\hat{Y}_{21,ecp}$  = 0 to be located in the vicinity of the band edges for the purpose of increasing the slope of the skirt, according to the specification, and vary the important physical dimensions until the goal is achieved. The TZ points where  $Y_{21,seq}$  is equal to  $-Y_{21,ccp}$  are shown. These frequency points are shown to be the same TZs of the Sparameters. In addition, the skirt becomes much steeper by more than 10 dB, owing to  $TZ_{\rm H1}.$  This is made possible with the physical dimensions shown in **Table 3**.

# TABLE III PHYSICAL ELEMENT VALUES OF THE PRELIMINARY CT ZOR BPF

Name	Value (mm)	Name	Value (mm)
L1	18.1	G1	2
L2	16.9	G2	0.8
L3	4.1	Le	2.5
W	0.1	Li	0.8

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300 W				SGN2935-	300D-R	
			EGN	131B200IV	-R	
200 W		EGN29B200IV-R				
	EGN13B200IV-R	EGN28B2	200IV-R			
150 W			SGN	2933-150[	)-R	
				EGI	N33B100I	V-R
100 W			EGN	131B100IV	-R	
100 W		EGN	29B100IV-	·R		
	EGNB090MK	EGN28B1	100IV-R			
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100 W	EMO	C2933L10	11R	

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If the preliminary shape of the proposed CT ZOR bandpass filter is examined, there is still room for reduc-

L3 W

L2

L1

L1

▲ Fig. 6 Final, folded CT ZOR bandpass filter.

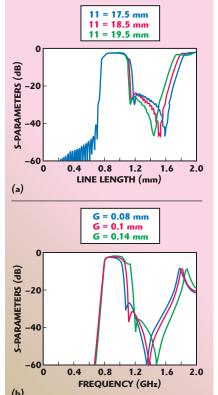
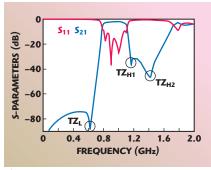


Fig. 7  $S_{21}$  vs. line length of the CCP in the CT (a), vs. the gap of the interdigital lines (b).



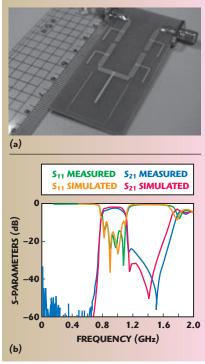
 $\blacktriangle$  Fig. 8 Simulated  $S_{11}$  and  $S_{21}$  of the final CT ZOR bandpass filter.

ing its total length. The preliminary structure can be folded with reference to ZOR three, while not distorting the

previous frequency behaviors and the improved skirt. Figure 6 is the folded version of the preliminary structure of the proposed CT ZOR bandpass filter. Obviously, it undergoes a change in  $S_{21}$  and  $S_{11}$ , due to the accompanying structural change in  $IRC_{2,3}$ ,  $IRC_{3,4}$ , etc. So it is inevitable to

correct the bandpass filter through another optimization.

As shown in **Figure** 7,  $S_{21}$  is mainly influenced by L1 in terms of the bandwidth and skirt, due to change of  $TZ_{H1}$ , and slightly by L2 and L3. Simultaneously, the variation of the interdigital lines' gap affects the TZs more seriously. With these observations, other geometrical parameters are adjusted to provide the optimal performance. They are finalized as Li = 0.8 mm, Lc = 1.6 mm, L1 = 18.6 mm, L2 = 16.9 mm, L3 = 4.1 mm, G1 = 2.3 mm, G2 = 0.8 mm, G3 = 0.45 mm, W = 0.1 mm. As is shown in **Figure** 8, the passband



▲ Fig. 9 Photograph of the fabricated filter (a) and measurements vs. 3D EM simulation (b).



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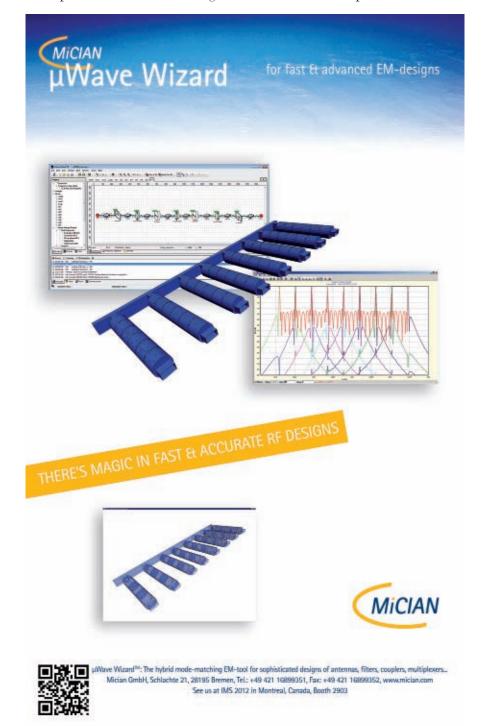
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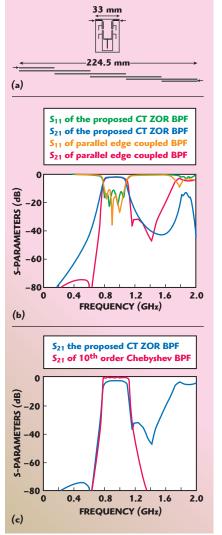


is obtained as specified before, and the insertion loss and return loss are 1.2 dB and 15 dB, respectively. Especially,  $S_{21}$  has an attenuation of greater than 20 dB at  $f_{ue}$ +50 MHz by creating TZs. Including this finding, the 3D EM analysis results, as well as circuit simulation, are validated by comparison with the measurement of the fabricated prototype.

Taking advantage of a simple microstrip structure and feasible geometric parameters, the manufacturing cost is very low. As shown in  $Figure\ 9$ , the area of the prototype is estimated to be  $74\times33$  mm, which is small for a UHF-band printed RF component. The measurements meet the target specifications and agree well with the 3D EM simulation, without manual tuning at the time of testing. The passband has an insertion loss better than 2 dB and the return loss is better than 15 dB. The sharp skirt is achieved

with  $S_{21}$  greater than 20 dB at the specified frequency point. Mentioning the insertion loss, it is very low despite using FR-4 as a lossy and cheap substrate. Lastly, to clearly show the advantages of the proposed CT ZOR filter over the conventional methods, the total size, passband performance and skirt are compared between the two cases. Apparently, the proposed CT ZOR bandpass filter is smaller than 1/7 of the parallel edge coupled bandpass filter as compared in *Figure* 10. The proposed filter has a much steeper skirt than the conventional filter. Furthermore, to find out how high the order of a conventional filter should be to have the same frequency selectivity as the proposed filter, it is uncovered that the slope of a 10th order conventional Chebyshev filter is the closest to the proposed filter. In





▲ Fig. 10 Comparison of sizes (a), S-parameters (b) and skirt (c) of the proposed and conventional filters.



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other words, the proposed filter has five resonators, but its effect is equivalent to the 10<sup>th</sup> order Chebyshev as:

$$S_{21}^{\text{conv.}}(s) =$$

$$\frac{b_9 s^9 + b_8 s^8 + \dots + b_2 s^2 + b_1 s + b_0}{s^{10} + a_9 s^9 + \dots + a_9 s^2 + a_1 s + a_0}$$
(8)

where the coefficients are  $a_9$  = 1.14,  $a_8$  = 3.15,  $a_7$  = 2.71,  $a_6$  = 3.44,  $a_5$  = 2.14,  $a_4$  = 1.53,  $a_3$  = 0.63,  $a_2$  = 0.24,  $a_1$  = 0.049,  $a_0$  = 0.0059,  $b_9$  =  $b_8$  =  $b_7$  =  $b_6$  =  $b_5$  =  $b_4$ 

=  $b_3$  =  $b_2$  =  $b_1$  = 0.0 and  $b_0$  = 0.0059. The indication is that a very high rate of miniaturization is achieved by the function of the  $10^{\rm th}$  order filtering from the physically fifth order filter.

### **CONCLUSION**

This article proposed a bandpass filter made very compact by implementing the CRLH ZORs and their coupling and forming a CT to have a steep skirt for high frequency selectivity. First, an in-line ZOR bandpass

filter was designed as the initial step, whose total size is nearly 20 percent of the parallel-edge coupled filter. Second, the CT and its TZs were provided for improving the skirt of the initial ZOR filter. As a result, with the insertion loss better than 1.5 dB and the return loss better than 15 dB, the sizereduction effect and the skirt of the proposed filter were 24 times smaller than even a fourth order parallel-edge coupled filter and as sharp as a 10<sup>th</sup> order Chebyshev filter, respectively. The simulation and measurements validated the proposed design method, and the CRLH ZOR properties were proven by the no-phase variation electric field and dispersion diagram.

### **ACKNOWLEDGMENT**

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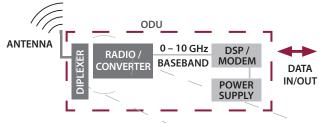
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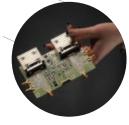
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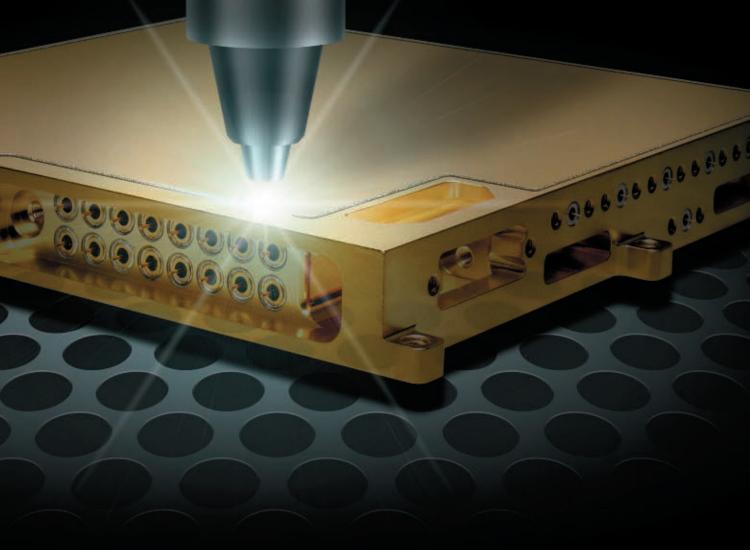
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# Quarter Substrate Integrated Waveguide Resonator Applied to Fractal-Shaped BPFs

A quarter substrate integrated waveguide resonator (QSIWR) and a fractal-shaped defected structure (FDS) are used to design miniaturized substrate integrated waveguide (SIW) bandpass filters. With the QSIWR, a conventional SIW filter can be reduced in size by approximately 75 percent and the size can be further reduced with FDS. Using QSIWR and FDS, a type of one-pole and a type of two-pole bandpass filters are proposed and optimized. The two-pole bandpass filter has more merits, such as a simple structure, compact size and an extra transmission zero in the upper stopband. The measured and simulated results of a two-pole filter are in good agreement.

In recent years, there has been a growing interest in the SIW technology, <sup>1-8</sup> which has the advantages of light weight, high power capacity and easy integration with other planar microwave circuits. But, compared to microstrip circuits, the SIW circuits are of larger sizes, especially in low microwave frequency bands. By using half mode substrate integrated waveguide (HMSIW)<sup>3-6</sup> and substrate integrated folded waveguide (SIFW)<sup>8</sup> structures, the total size of a SIW is nearly reduced by a half, but still keeps comparable performances.

Many kinds of miniaturized filters<sup>4,5,7</sup> and antennas<sup>6</sup> have been proposed using these technologies. The propagation modes of SIW are similar to those of a rectangular waveguide, so cavity resonators are the basic shapes used in the design of SIW filters. Utilizing the sym-

metry of SIW, the HMSIW is obtained by cutting the SIW along the perfect magnetic wall. It still keeps half of the field distribution of the dominant mode TE<sub>10</sub>. The same idea can be applied to shrink the square SIW resonator. By cutting the square SIW resonator along magnetic walls, a quarter SIW resonator (QSIWR) is derived. Using QSIWR, two types of bandpass filter are proposed, achieving approxi-

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### Technical Feature

mately a 75 percent reduction in size compared to conventional ones. At the same time, the fractal-shaped<sup>9-11</sup> defected structures (FDS) are etched in the QSIWR, which can further reduce the filters' size and improve their selectivities.

### **QUARTER SUBSTRATE INTEGRATED WAVEGUIDE RESONATOR**

In **Figure 1**, if the width of the rectangular resonator is equal to the length a, the TE<sub>101</sub> mode can be expressed as follows, which is the same as the square SIW resonator.<sup>1</sup>

$$\begin{cases} E_{y} = -j\frac{\omega\mu a}{\pi}H_{m}\sin\left(\frac{\pi}{a}x\right)\sin\left(\frac{\pi}{a}z\right) \\ H_{x} = -H_{m}\sin\left(\frac{\pi}{a}x\right)\cos\left(\frac{\pi}{a}z\right) \\ H_{z} = H_{m}\cos\left(\frac{\pi}{a}x\right)\sin\left(\frac{\pi}{a}z\right) \\ E_{x} = E_{z} = H_{y} = 0 \end{cases}$$
(1)

According to Equation 1, the magnetic field intensity H perpendicular to the Plane AA' (x = z) and the plane BB'(x = -z) are similar, so at the fundamental resonant mode (TE<sub>101</sub>), the AA' and BB' planes are equivalent to perfect magnetic walls. On the condition that the substrate is very thin, by cutting along AA' and BB', quarter SIW resonators are left. The QSIWR's open sides are nearly equivalent to perfect magnetic walls. As shown in Figure 2, comparing with the electric fields of SIW and QSIW, the field is kept almost undamaged. There is only a small wave leakage along two magnetic walls. So the OSIWR can be used to design various cavity filters with 75 percent reduction in size.

### FRACTAL ONE-POLE FILTER **USING QSIWR**

In order to verify the resonant characteristics of QSIWR, first a new fractal one-pole filter is designed, which is shown in Figure 3. The geometry of QSIWR is a right angled isosceles triangle (RAIT). Two microstrip feed lines are at the center of each right-angle side. The 50  $\Omega$  microstrip line with  $\varepsilon_r = 2.2$  and loss tangent of 0.0009, height h = 0.508 mm, conductor strip width w = 1.58 mm is chosen for all filters. At the same time, the di-

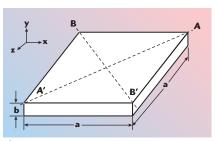


Fig. 1 Schematic of the square waveguide resonator.

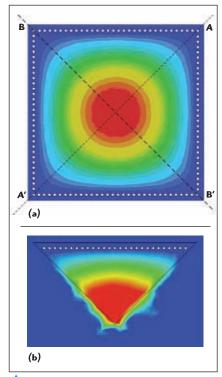


Fig. 2 Electric field distribution of a square SIW (a) and QSIWR (b).

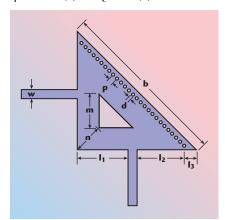


Fig. 3 One-pole QSIWR with a fractalshape structure.

ameter of the vias is d = 0.5 mm and the pitch between vias is p = 1.1 mm. The resonant frequency is mainly decided by the hypotenuse length b. To lower the resonant frequency, a RAIT

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- RF and Wireless Concepts and Terminology
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224-4472	Power Conversion & Regulation Circuits for VLSI Systems	.Aug 20-23	Jul 16.\$1,695.00	\$1,895.00
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San Jose,				
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230-4510				
223-4511				
135-4512	RF Measurements:Principles & Demonstration	.0ct 15-19	Sep 10.\$2,295.00	\$2,495.00
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199-4513	RF and Wireless Transceiver Design & Evaluation Techniques	Nov 5-9	0ct 1.\$1,995.00	\$2,295.00
227-4514	Wireless LANs	.Nov 5-7	Oct 1.\$1,495.00	\$1,595.00
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234-4516	RF and Wireless Concepts and Terminology			
027-4519	Understanding Digital Signal Processing (DSP)			
181-4520	Monolithic Microwave Integrated Circuit (MMIC) Design	.Jan 16-18, 20	013 Dec 10.\$1,495.00	\$1,595.00
San Dieg	o, CA February 2013	Dates	Earlybird Deadline & Price	Reg. Price
	Antennas & Propagation for Wireless Communications			
	Applied RF Techniques I			
	Practical Digital Wireless Signals			

### **Course Descriptions**

### WEB - Web Class, AUG, OCT, NOV, DEC - San Jose, CA, FEB - San Diego, CA

### 214 Advanced Radio System Architectures

The ideas associated with sampling and digital signals that revolutionised modulation systems and are now revolutionising radio system design. This course continues the theme of block diagram rather than circuit diagram design, presenting an up to date view on concepts for advanced radio systems that incorporate digital signal processing at RF frequencies and the concepts of software defined radio. It is a practical approach for technical professionals to understand the latest designs and architectures for radio systems that include DSP. Aug

### 037 Antennas & Propagation for Wireless Communications

This three-day course provides participants with comprehensive coverage of a wide variety of antenna and propagation topics. The course provides an understanding of basic antenna property definitions, antenna design fundamentals and considerations, numerous antenna types and RF propagation fundamentals. The course also provides an overview of how antenna properties and propagation characteristics affect communication system performance. Topics covered include antenna fundamentals, basic antenna types, elementary antennas, electrically small antennas, microstrip patch antennas, low profile antennas, aperture and reflector antennas, circular polarized antennas, antenna arrays, propagation channel characteristics, and an overview of different antennas used in

today's wireless communication devices and markets. Feb

### 86 Applied RF II: Advanced Wireless and Microwave Techniques

This five-day course provides participants with an in-depth examination of advanced RF and microwave design techniques. Antennas and filters are covered briefly, followed by a detailed discussion of figures of merit. Mixers and oscillator designs are also evaluated. Considerable attention is devoted to defining, classifying, and improving the efficiency and linearity of power amplifiers. Numerous design examples are provided for participant exploration. Aug

### 001 Applied RF Techniques I

Switching from traditional definitions based on voltages and currents, to power-flow concepts and scattering parameters, the course has smooth transition into the wireless domain. We review S-parameter measurements and applications for both single-ended (unbalanced) and balanced circuits and have a brief introduction to RF systems and their components. Impedance matching is vitally important in RF systems and we use both graphical (Smith Chart ) and analytical techniques throughout the course. We also examine discrete and monolithic component models in their physical forms, discussing parasitic effects and losses, revealing reasons why circuit elements behave in surprising manners at RF. Aug,Feb

### 212 Behavioural Modeling & Digital Pre-Distortion of RF Power Amplifiers

The goals of RF power amplifier design are high efficiency and linearity. With modern cellular communications modulation formats such as LTE



and WCDMA these goals are difficult to achieve simultaneously with traditional RF PAs, and high-efficiency architectures such as Doherty, Envelope Tracking, and so forth are becoming more commonplace. These PAs require an additional linearization system to achieve the mandated linearity specifications. The emergence of high-speed digital signal processing techniques has enabled the linearization to be accomplished in the digital signal domain, and digital pre-distortion (DPD) is now the preferred linearization technique.

This course explains the nonlinear behaviour of RF power amplifiers, developing general modeling techniques to describe the nonlinearities and memory effects. A system-level approach to the modeling and linearization of the PA is adopted, and techniques for implementation of DPD in practical situations are described. **Dec** 

### 140 EMC/Shielding/Grounding Techniques for Chip & PCB Layout

This seminar discusses techniques for identifying the sources of unwanted coupling and radiation, and systematic approaches for their minimization. Web

### 230 EMI/EMC Design and Troubleshooting

This course covers the methodology of designing an electronic product to minimize the possibility of having problems of electromagnetic interference (EMI) or Electromagnetic Compatibility (EMC). Useful techniques for troubleshooting an EMI/EMC problem are presented to help with products where problems exist. **Oct** 

### 223 Fundamentals of LTE, HSPA, & WCDMA

Understanding the evolution of wireless data transmission from 3G to 4G technologies is critical to today's commercial component and system vendors. This comprehensive three day program covers the key technologies in a clear and concise manner. **Oct** 

### 228 GaN Power Amplifier Design

This course introduces attendees to the GaN transistor, its properties, various structures, discrete devices and MMIC sources, including the latest GaN power amplifier (PA) design techniques. The properties of GaN will be presented showing the advantage of these devices over GaAs and Si. GaN HEMT transistors will be shown delineating the various geometries, semiconductor processes and structures with associated breakdown voltages, power capability, gain, efficiency, and frequency performance. Guidelines for reliable operation will be presented considering device junction temperature including thermal management techniques. Web

### 229 Introduction to Impedance Matching

The need for impedance matching is rooted in basic AC circuit analysis principles. In basic terms, maximum power transfer occurs when the current and voltage are in phase. This workshop examines the ins and outs of delivering the most power possible to an RF load. Q factor and its effect on matching network bandwidth are also described. Web

### 181 Monolithic Microwave Integrated Circuit (MMIC) Design

The successful design of monolithic microwave integrated circuits (MMICs) is the fruit of a disciplined design approach. This three-day course covers, in detail, the theory, and practical strategies required to achieve first-pass design success. Specifically, the course covers the monolithic implementation of microwave circuits on GaAs substrates including instruction on processing, masks, simulation, layout, design rule checking, packaging, and testing. Numerous design examples are provided with emphasis on increasing yield, and reliability. Jan San

### 220 Phase Noise and Jitter

Timing-related problems associated with signal sources are one of the major bottlenecks in designing today's highly complex systems. Over many decades, jitter has been extensively studied and utilized to characterize timing inaccuracies in both digital and analog systems. Conversely, phase noise has been exclusively used in RF systems to represent frequency or phase inaccuracy. For both timing and frequency sensitive systems, phase noise measurement is emerging to be the most accurate method of characterizing all types of signal sources (RF, analog or digital). This

short course covers the fundamentals of phase noise and jitter, which ultimately set the limit to PLL performance in applications such as frequency synthesis, serial data communication and clock/data recovery. Simple techniques to model phase noise at the circuit component-level and relate it to the overall phase noise and jitter performance of PLLs are presented. The course will also provide a detailed analysis of the different phase noise measurement techniques along with in-depth noise floor analysis. The focus throughout this course will be on providing practical measures utilizing numerous real life examples. Web

### 216 Power Amplifier ABC's

This course aims to bring participants up to speed on the basics of RF power amplifier design and operation in the shortest possible amount of time. Considerable attention is devoted to defining, classifying, and improving the efficiency and linearity of power amplifiers. Numerous design examples are provided for participant exploration. The class offers approximately one day's worth of material, but is typically offered in five 90-minute sessions via web-classroom. Web

### 224 Power Conversion & Regulation Circuits for VLSI Systems

Developing power conversion/regulation solutions for VLSI systems and mixed-signal analog/RF System-on-Chip (SoC) types of loads require engineers with solid background in both traditional power converters design as well as analog/RF mixed-signal VLSI design. Power conversion/regulation circuits with such a VLSI and SoC focus are rarely covered in graduate or undergraduate power electronics courses. With the growing demand in semiconductor industries for expertise in this area, there is a serious shortage in engineers who have the necessary background combination to design efficient and cost-effective solutions for such loads. This course will introduce the fundamental principles of power conversion/regulation circuits such as Linear/switching regulators and battery chargers used in VLSI systems. This includes: Architectures, Performance metrics, characterization, stability and noise analysis, practical implementations, on-chip integration issues, and design considerations for portable, wireless, and RF SoCs. Aug

### 232 Practical Digital Wireless Signals

This three day course is designed to provide all participants with a physically intuitive understanding of wireless communication signals and why they work the way they do. With the growing impact of wireless communications on the basic operation of society, the need for a more general understanding of the basis for this technology is more important than ever. This course approaches wireless communications signals through the window of physics and physical principles. While a solid understanding of the mathematical theory of wireless communications signals is essential for detailed system design and analysis, the fundamental choices in system application and approach are often best approached physically. We do not shun math in this presentation, but instead of using math as the presentation base we instead use it as a follow up illustrator of the principles discussed. Feb

### 231 Radio Frequency Basics for Electronics Professionals This course covers the fundamentals of high frequency (RF) design

This course covers the fundamentals of high frequency (RF) design for engineers and technicians in the electronic market. The course is not intended for telecomm specialists but for design, production and installation engineers who need to increase or review their curriculum with radiofrecuency technology.

Many products, non related classically with RF, give a growing importance to high frequency techniques: products where radio is included through ZigBee or Bluetooth, electromagnetic interference problems (EMI/EMC), high speed digital circuits, signal integrity, high speed switching (power) circuits, switching power supplies, filters, need for shielding in both susceptibility and emissions, spectrum analysis, RF instruments, etc. Oct

### 42 RF and High Speed PC Board Design Fundamentals

This three-day course enables practicing engineers and CAD technicians to develop design rules for RF and high-speed designs, choose an optimal design tool, and organize the design process to most efficiently execute the design that will insure circuit performance, and minimize costs and production time. **Dec** 



### 234 RF and Microwave Transistor Tutorial

This 2 hour tutorial provides microwave circuit designers with an overview of their "toolkit" of semiconductor devices. We look at functional descriptions of the basic semiconductor devices: the P-N junction, the bipolar transistor and the FET. Further material describes basic transistor operation, using heterojunctions for higher performance, as well as the effects of material properties on performance and reliability. Web

### 234 RF and Wireless Concepts and Terminology

This two-day day course provides nontechnical professionals with a firm understanding of basic RF principles and technical concepts. RF technology, wave propagation and transmission techniques will be characterized for various performance requirements. This course will also convey a conceptual understanding of RF wireless systems and how they work for the multiple wireless standards. All explanations use simple physical descriptions without complex mathematics. Dec

### 199 RF and Wireless Transceiver Design & Evaluation Techniques

This 5-day course provides technical professionals with the design concepts and development tools required to architect RF transceivers for most wireless applications. The course is intended for working engineers that are in the design, test or support phase of new transceiver technology.. Also, Critical system specifications will be discussed based on worldwide standards and an in-depth review of transceiver configurations will be evaluated. The use of RF simulation tools will be used to show design concepts and the trade-offs between modulation techniques and RF performance. RF air interface requirements and specifications will be presented for various wireless standards including LTE and systems like GPS, Bluetooth, 802.11, wideband CDMA, EDGE and others. Radio architectures based on digital modulation techniques like OFDM, OFDMA, SC-FDMA, QAM, BPSK, QPSK, GSM, 8PSK, GFSK will be analyzed using simulation tools and design examples. Designs of the latest architectures including 4G LTE transceivers will be presented with class participation using the lasted CAD design tools. Finally, transceiver test and troubleshooting procedures from RF to baseband will be described. Nov

### 59 RF Fundamentals

This course provides circuit-level designers with the essential concepts needed to work effectively with high frequency electronics. Participants gain analytical, graphical, and computer-aided techniques to analyze and optimize RF circuits in practical situations. The course addresses linear active circuit design, focusing on stability, bandwidth, and noise considerations. Web

### 135 RF Measurements:Principles & Demonstration

This 5-day lecture-based course explains essential RF measurements that must be made on modern wireless communications equipment - mobile/smart phones, wireless LANs, GPS navigation systems, and others. Current models of the essential test instruments will be explained and demonstrated, including vector network analyzers, power meters, spectrum analyzers, digitally modulated signal generators and vector signal analyzers. All of the measurements will be demonstrated on actual RF wireless components including power amps, LNAs, mixers, upconverters, and filters. These measurements will include traditional tests of power, gain, group delay, S parameters, AM to PM, intermodulation products, harmonics and noise figure. The unique measurements of wireless communications will then be made with PSK and FSK digitally modulated signals including spectral regrowth, constellation diagram distortion, error vector magnitude (EVM), and bit error rate. Oct

### 222 RF Power Amplifier Techniques

Power amplifiers are crucially important in determining a communications system cost, efficiency, size, and weight. Designing high power / high efficiency amplifiers that satisfy the system requirements (bandwidth, linearity, spectral mask, etc.) is challenging. It involves difficult trade-offs, proper understanding of the theory, and careful attention to details. Additionally, designing, building, and testing power amplifiers usually pushes test equipment and lab

components to their limits and frequently results in damage to the circuit or lab equipment. This course will examine the different aspects of this challenge with emphasis on hand-on exercises and practical tips to build power amplifiers successfully. Aug

### 27 DSP -Understanding Digital Signal Processing

This three-day course is the beginner's best opportunity to efficiently learn DSP. Intuitive, nonmathematical explanations and well-chosen examples develop the student's fundamental understanding of DSP theory. The practical aspects of signal processing techniques are stressed over discrete system theory. Participants will leave with a collection of tricks-of-the-trade used by DSP professionals to make their processing algorithms more efficient. Public course attendees will receive a copy of the book - *Understanding Digital Signal Processing* by Rick Lyons **Dec** 

### 227 Wireless LANs

This three-day course is an experiment-oriented course that integrates topics at the MAC layer (and above) of Wireless LANs (WLANs) and Wireless Personal Area Networks (WPANs). The course emphasizes hands-on learning through experiments and case studies. It will offer attendees the ability to conduct laboratory experiments and design projects that cover a broad spectrum of issues in WLANs and WPANs. The characteristics and operations of IEEE 802.11a/b/q/n WLANs will be described as well as that of Bluetooth WPANs. Laboratory experiments will be conducted to show the tradeoffs of the virtual carrier sensing mechanism, observe interference issues with other devices operating on the ISM band, describe Mobile Ad-hoc NETwork (MANET) operations and routing protocols, configure secure infrastructure and MANET WLANs, deploy hotspots, and use modeling, simulation, and emulation tools to evaluate WLANs (including system in the loop capabilities). Real infrastructure and MANET WLANs will be deployed and configured in class under different network scenarios. Different tools and techniques will be introduced to monitor, measure, and characterize their performance (and realize the tradeoffs). Known techniques to attack WLANs will be shown and proper security practices to avoid well-known threats will be discussed. All concepts will be summed up in an experiment that aims at deploying a secure hotspot Nov



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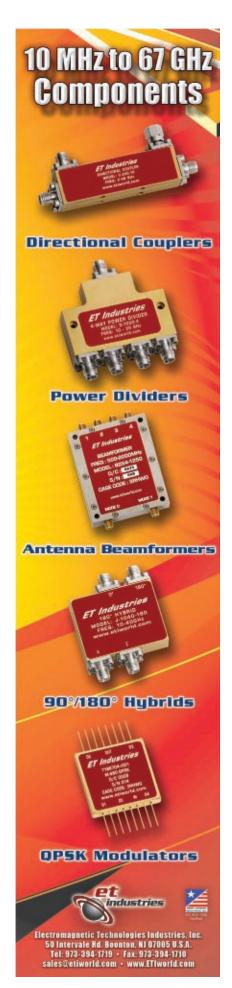


TABLE I DIMENSIONS OF THE ONE-POLE				
FILTER WITH QSIWR				
Symbol	Value (mm)			
W	2.4			
p	1.1			
d	0.5			
b	30			
m	6			
n	5.5			
$l_1$	9.1			
$l_2$	8.4			
$l_3$	1.9			

defected structure is etched in the center of its upper metal plane. The final dimensions are listed in *Table 1*. As shown in *Figure 4*, comparing with the filter without fractal structure, the resonant frequency of the filter with fractal structure shifts to a lower frequency, which is approximately 4.67 GHz, the –3 dB bandwidth is approximately 0.98 GHz. For only one cavity with one resonant mode, there is only one pole in the passband and the upper stopband is not satisfied.

### FRACTAL-SHAPED TWO-POLE FILTER USING QSIWR

To widen the usefulness of the QSIWR, a kind of two-pole filter is proposed. Figure 5 depicts the main configuration of this filter. First, two identical QSIWR are set back to back. With the central metal vias removed, the remaining vias act as the inductive iris. The microstrip feed lines are placed at the symmetrical sides of the filter. The resonant frequency  $f_0$  of this filter is specified at 4.5 GHz with a fractional bandwidth (FBW) of 12 percent. A two-order Chebyshev lowpass filter with passband ripple of 0.01 dB is chosen as the prototype. 12 The main factors of the two-pole filter are as follows:  $M_{12} = 0.280\overline{47}$ ,  $Q_{ei} =$ 3.74083,  $Q_{eo} = 3.74089$ .

 $M_{12}$  denotes the coupling coefficient between two neighbor resonators and  $Q_{ei}$  and  $Q_{eo}$  are the input and output external quality factor, respectively. Keeping the diameter of the vias d and the pitch p between vias unchanged, the other size parameters of the two-pole filter are as follows:  $l_4$  = 7.5 mm, e = 9.82 mm. As shown in **Figure 6**, in the whole passband, the

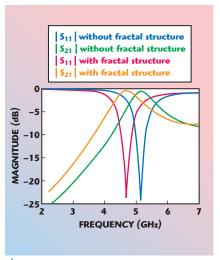


Fig. 4 S-parameters for the one-pole QSIWR filters, with and without fractal structure.

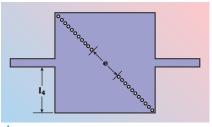


Fig. 5 Two-pole bandpass filter with OSIWR.

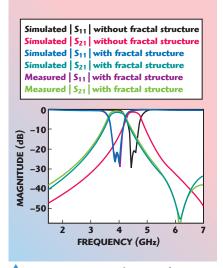


Fig. 6 S-parameters for two-pole QSIWR filter with and without fractal structure.

insertion loss is approximately 1.2 dB and the return loss is better than 20 dB from 4.40 to 4.62 GHz, the -3 dB bandwidth is approximately 0.6 GHz. The rejection is improved, especially at the upper stopband.

To make the filter more compact, Sierpinski triangles are etched in this two-pole filter. Its fractal dimension

# make it

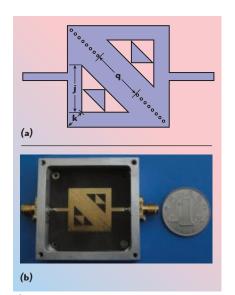
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▲ Fig. 7 Two-pole bandpass filter with fractal-shape QSIWR (a) layout and (b) photograph.

is D = In 3/In 2 = 1.585.<sup>11</sup> As shown in *Figure* 7, three identical RAITs are etched in the center of each QSIWR. The fractal structure has a distinct effect on the transmission

zero of the right side, which makes the filter have a sharp attenuation in the upper stopband. By optimizing the distance q equivalent to two inductive irises and the length i of the right-angle side, the passband shifts to a lower frequency dramatically. The dimensions of the RAIT are as follows: k = 6.52 mm, q = 14.1 mm,j = 8 mm. The simulated and measured results agree well, as shown in Figure 7. With the dimensions of OSIWR unchanged, the resonant frequency of the filter using fractal structures is 3.86 GHz. One transmission zero with an attenuation of 56.9 dB is implemented at 6.13 GHz, which highly improve the selectivity of the upper stopband. The fractal structure plays an important role in improving the performance of the two-pole filter; it perturbs the fields of QSIWR and couples well with the two QSIWRs. This fractal structure affects the filter's transmission zero, bandwidth and return loss in the passband. At the same time, it makes the filter more compact.

### CONCLUSION

In this article, according to the magnetic walls theory, a new quarter substrate integrated waveguide resonator is first proposed. Then a fractal-shaped structure is etched off the QSIWR, which makes the QSIWR's resonant frequency shift to a lower frequency. Then, a fractal-shaped QSIWR is used to design a two-pole bandpass filter. Compared to the filter without a fractal-shaped structure, the fractal-shaped one has many advantages, such as lower resonant frequency, more compact dimensions and high selectivity in the upper stopband. In short, the proposed fractal-shaped QSIWR can significantly shrink the filter's size and improve the filters' selectivity, which extend the usability of these shrunk resonators in filter applications.

### **ACKNOWLEDGMENT**

This work is supported by the Fundamental Research Funds for the Central Universities (2010QNA49).



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# Signal Generators Provide Perfect and Precisely Imperfect Signals

R technology marches on at a furious rate, whether it is for wireless communications, aerospace/defense, or everfaster wireless networking applications. Test equipment performance and capabilities have been driven forward at a similar pace. Interestingly, one of the more remarkable developments in Agilent's new X-Series RF signal generators is unique technology that provides "precisely impaired" signals. Available in analog and vector modulation models – from the pure and precise MXG to the cost-effective EXG – these new instruments provide both perfect and precisely

imperfect signals.

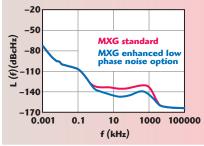


Fig. 1 The MXG's phase noise, different levels of phase noise performance are available as options.

### PUSHING THE PERFORMANCE ENVELOPE

Development of new RF technologies depends on test equipment that pushes the performance envelope. A prime example of this is the MXG, which is now setting new standards in phase noise and spurious performance, signal purity, modulation bandwidth and output power.

The MXG uses a new triple-loop synthesizer design that leverages Agilent's own fractional-N ASIC to achieve industry-leading phase noise and spurious performance. As shown in *Figure 1*, several levels of optional phase noise performance are available to optimize price/performance for different applications. At 1 GHz and a 20 kHz offset, the standard MXG unit has a phase noise of -134 dBc/Hz. When options UNX/UNY are employed, phase noise improves to -146 dBc/Hz. Spurious performance from the multi-loop implementation is -96 dBc/Hz (all figures typical).

The synthesizer architecture pays similar dividends in terms of broadband noise, being reduced to –163 dBc/Hz at 1 GHz for both the MXG and the new cost effective EXG. All of these specifications are improved by 10 dB or more from Agilent's previous generation ESG signal generators. Other measures of signal purity have also improved. ACPR, for example, is as good as –73 dBc for W-CDMA (TM1, 64

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DPCH). This signal purity is achieved without a loss of frequency agility. Switching speed for all X-Series signal generators is now specified at better than  $900~\mu s$  in list sweep mode.

Coupled with the signal purity of the new X-Series signal generators is their availability to deliver power. For applications such as amplifier test, pure signals must be supplied at high power levels to exercise and quantify nonlinearities such as harmonics, intermodulation and compression. To help engineers avoid the expense and inconvenience of external amplifiers, the MXG specifies an industry leading +24 dBm (27 dBm typical) to 3 GHz and +19 dBm to 5 GHz. This combination of power and purity is made possible by Agilent's own low-loss pin diode electronic attenuators that also offer extended life and reliability in manufacturing environments where they may be cycled very frequently.

# A NEW STANDARD FOR MODULATION ACCURACY AND WIDE BANDWIDTH Data rates for mobile con

Data rates for mobile communications and wireless networking continue to rise rapidly, leading to a combination of dense constellations and wide modulation bandwidths. The IEEE 802.11ac standard is a prime example, promising gigabit speeds through the use of 256QAM modulation at bandwidths up to 160 MHz. The MXG uses advanced modulator circuits and innovative calibration techniques to overcome the I/Q and frequency response problems that generally worsen with increasing bandwidth. The result is a modulated signal that removes any doubt about the source or magnitude of a system's modulation error.

Pushing technology to the next level often rules out the use of off-theshelf ASICs. The IQ modulator in the vector MXG and EXG models prove this fact. Developed and manufactured by Agilent, it sits at the core of a modulation section that delivers industry leading ACPR over bandwidths as wide as 160 MHz internally, and up to 300 MHz from external sources. This modulation section is linearized by an internal calibration source and algorithm that provides vector correction factors to a real-time baseband processor. The result is an 802.11ac 256OAM error vector magnitude (EVM) of 0.4 percent (typical) over 160 MHz in the MXG and 80 MHz in the EXG.

Built-in channel calibrations also provide full vector correction from the modulator through RF output. This ensures a high dynamic range and flatness of ±0.2 dB across the MXG's 160 MHz bandwidth and EXG's 120 MHz bandwidth. Moreover, no user intervention (e.g., manual IQ adjustment) is required. Wide modulation bandwidth and high dynamic range provide user benefits even when individual signals are narrower. The crowded nature of today's spectral environment means that receivers must cope with problems such as adjacent channel interference and multiple types of blocking. A modern smartphone, for example, can have three or more transceivers operating at the same time, and often operates close to other similarly complex devices. The





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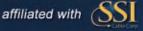
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### WIDE REAL-TIME SIGNAL GENERATION AND DEEP ARB MEMORY

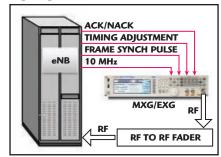
Both real-time baseband genera-

tion and arb playback memory approaches have advantages in creating modulated signals; some applications are better satisfied by one approach than the other. The MXG and EXG vector models combine these baseband generators in one unit, ensuring the best approach is always available to the user.

The real-time baseband generator and its processor-accelerator support a large number of applications in cellular communications, wireless networking, audio/video broadcasting and navigation (e.g., GPS and GLONASS). Real-time modes also include custom or flexible modulation types, including dense constellations up to 1024QAM. The real-time mode allows for creation of complex signal scenarios with very long durations. For satellite navigation, the MXG and EXG can generate signals representing up to 32 line-of-sight GPS/GLONASS satellites, including real-time control of satellite visibility and power for up to 24 hours without repeating.

The feedback loops in mobile wireless systems also benefit from real-time generation, where closed-loop testing is used to evaluate the throughput of real-world channels. An example configuration is shown in *Figure 2*. In testing such as LTE HARQ, the X-Series signal generators can receive TTL-level feedback signals and reconfigure the transmission signal while maintaining the link. This enables more realistic testing of throughput over impaired channels.

The other mode available in the X-Series is an extremely deep arb memory. Playback of baseband data from a deep arb memory is a flexible way to generate many different signal types at RF. The signals for the arb memory are typically generated by a PC program, such as Agilent's Signal Studio, that is available for many wireless, video and navigation standards like LTE, W-CDMA, HSPA, 802.11, DVB-T/H, GPS and GLONASS. The MXG and EXG provide up to 1 GSample and 512 MSamples of memory, respectively, for a capability that exceeds conformance requirements and can, in some cases, offer an alternative to real-time signal generation.



▲ Fig. 2 Transistor-transistor logic (TTL) feedback signals control a real-time baseband generator in the RF source for closed-loop testing.

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RWP05080-10	500 ~ 600	46	47	53	56	55
RWP06080-10	600 ~ 700	43	47	53	56	55

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Part Number	Frequency (MHz)	Gain (dB)	Flatness (dB)	NF (dB)			Vd (V)		Package
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RADA-76PC909C	CH2:659	78	1.8	1.0	1.4	20@CH1	5	47 x 50.8 x 8	

### Switch

Part Number	Frequency (MHz)	I.L (dB)	Flatness (dB)	Isolation (dB)	P1dB (dBm)	OIP3 (dBm)	Vd (V)	Id (mA)	Package
SE902	50 ~ 3000	-0.5	-	-55	21	36	3 ~ 5	1	QFN4x4

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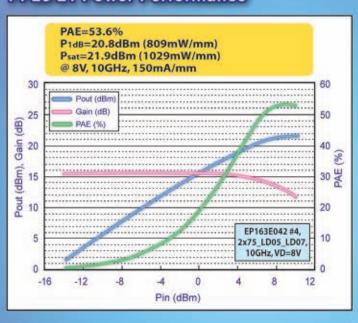
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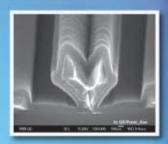


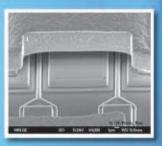
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Idmax (mA/mm)	720	650	460	480
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VDG (V)	9	10	19.2	20
ft (GHz)	130	85	65~72	32
Fmax (GHz)	175	180	160	85
PldB (mW/mm)	533.25 (3.5V)	670 (5V)	809 (8V)	587 (8V)
Psat (mW/mm)	764.3 (3.5V)	820 (5V)	1029 (8V)	851 (8V)
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### PRECISELY IMPERFECT SIGNALS: CUSTOMIZED PHASE NOISE

Real-time vector signal processing can modify or predistort signals to correct for system or channel problems, but can also be used to selectively degrade signals. While the typical purpose of a signal generator is to provide a clean stimulus or reference, they are also vital in testing a system's response to representative impairments.

The low phase noise of the MXG is not a benefit in all cases. Real-world systems must deal with phase noise in both continuous wave (CW) and modulated signals. Therefore, the ability of a signal generator to act as an adjustable and accurate substitute can shorten development time and reduce the chances (and resulting costs) of under- or over-performance. In the MXG, a real-time signal-processing

ASIC customizes phase noise levels for both CW and modulated signals. In an important innovation, phase noise can be adjusted to different levels at different offsets, including the steep slopes of close-in noise, the flat slopes of synthesizer pedestal noise and the shallow slopes of wide offset noise.

### **REDUCING THE COST-OF-TEST**

The total cost-of-test, especially over time, is far more complicated than the equipment cost. The X-Series signal generators were designed to minimize costs over their entire life cycle in real-world manufacturing. They begin by offering a range of choices to optimize performance, capability and cost.

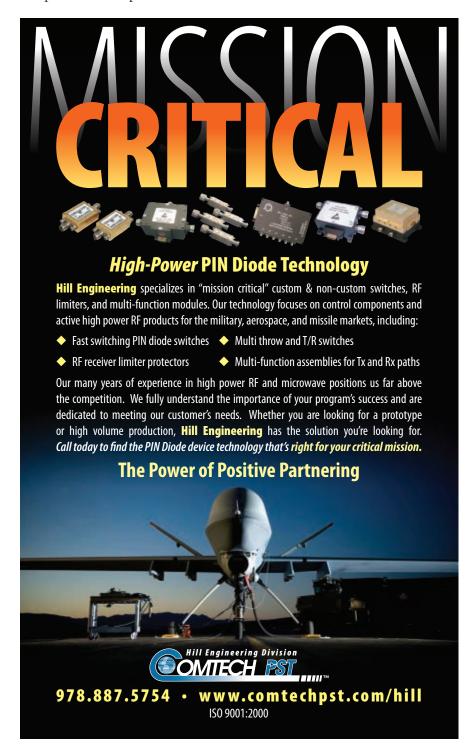
Multiple MXG and EXG models include both moderate- and high-performance generators with analog and vector capabilities, and different frequency coverage to match application needs. This flexibility supports agile manufacturing, where the flexible options and application software structure allow signal generators to be re-purposed to remain productive over a longer life.

Once in place, the ideal signal generator does its job forever with a minimum of attention. The low-loss, solid-state attenuators of the EXG/MXG make countless amplitude changes without wear, contributing to a three-year instrument calibration cycle. Unproductive downtime is minimized with self diagnostics, a refurbished assembly exchange program, and an innovative hardware design that requires no post-repair calibration or adjustment.

RF technology may be marching on at a furious rate, but the performance and capabilities of the new X-Series signal generators are definitely keeping pace. By pushing the envelope on performance, functionality and cost, they are now providing engineers with better choices for both design and manufacturing.



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# Single Chip AGC Solutions for Communications

automatic gain control (AGC) or automatic power control (APC) circuits are used primarily to maintain a constant power level in the signal chain of a communication transceiver. A simple AGC circuit involves attenuation, amplification, power detection and gain control mechanisms. In an AGC system, the average output signal level is fed back to adjust the gain to an appropriate level for a range of input signal levels. For example, without AGC, the audio level emitted from an AM radio receiver would vary depending on the received signal strength; the AGC effectively reduces the volume when the signal is strong and raises it when it is weaker. AGC algorithms

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▲ Fig. 1 Block diagram of a typical AGC solution implemented with discrete components.

often use controllers that can adjust the gain of the signal chain in inverse proportion to the error between desired and measured power levels. *Figure 1* shows a discrete implementation of an AGC circuit controlling gain in accordance with the power level detected via a feedback loop.

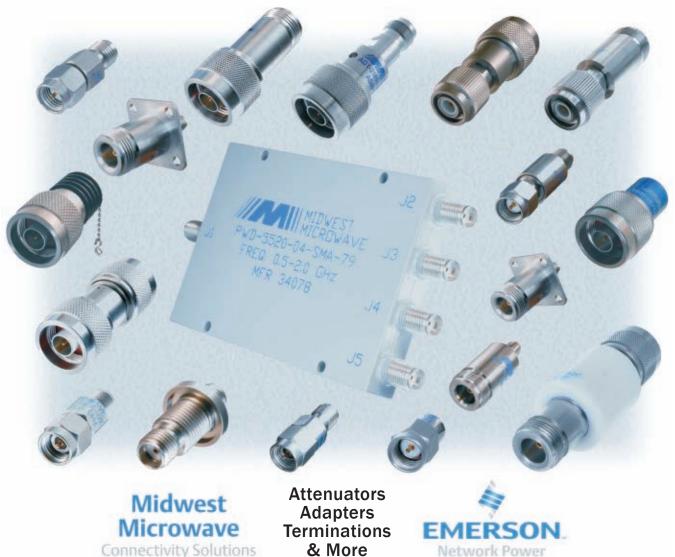
Unfortunately, AGC loops implemented with discrete components often suffer from a number of deficiencies. For example, the analog voltage variable attenuator (VVA) element in a discrete AGC loop often exhibits large OIP3 dips at certain control voltages, or OIP3 degradation as the attenuation is increased. Since the AGC loop is implemented with multiple discrete components, the power control accuracy is more sensitive to part-to-part and temperature variations. Additionally, each of these components often requires external circuitry that requires extra PCB space and further complicates the overall AGC loop design.

Hittite Microwave has developed a unique new product line of highly integrated analog AGC solutions that address many of the complex challenges of designing high performance AGC loops. *Table 1* summarizes the key specifications of these new products. The HMC992LP5E is an IF analog controlled variable gain amplifier (VGA) that operates from 50

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TABLE I									
HITTITE'S AGC SOLUTIONS									
Key Feature	HMC992LP5E	HMC993LP5E							
Operating Frequency Range	50 to 800 MHz	700 MHz to 3 GHz							
Linearity	+40 dBm OIP3 across entire attenuation range	+40 dBm OIP3 across entire attenuation range							
Gain Control Range (dB)	-10 to +38	-11 to +32							
Highly Flexible	Configurable with 1 or 2 attenuators	Configurable with 1 or 2 attenuators							
Power Detector Function	On chip	On chip							
Positive Analog Control Voltage (V)	0 to +5	0 to +5							
Noise Figure (dB)	6	7.6							
P1 dB (dBm)	19	25							
Supply Voltage (V)	+5	+5							
Supply Current (mA)	215	260							
Package	LP5 (5 $\times$ 5 mm SMT)	LP5 (5 $\times$ 5 mm SMT)							

to 800 MHz, and the HMC993LP5E is an RF analog controlled gain amplifier that operates from 700 MHz to 3 GHz.

Both the HMC992LP5E and the HMC993LP5E combine a high performance analog VGA core with a high speed power detector in a compact

5×5 mm plastic package for a complete AGC solution. The VGA core includes two identical voltage variable attenuators followed up by two gain block amplifiers and a high accuracy log detector. The HMC992LP5E and the HMC993LP5E offer a flexible architecture, where the VGA core

is configurable with 1 or 2 attenuators depending upon the dynamic range requirements. These devices can also be used either as standalone high performance VGAs in open loop configuration, or as a compact AGC solution in closed loop operation. The HMC992LP5E and HMC993LP5E AGC solutions are available in compact 25 mm² SMT packages and provide an excellent alternative to discrete AGC loops by reducing the complexity of the loop design, and the total number of components required.

The unique VGA core of the HMC992LP5E and the HMC993LP5E exhibits a well-balanced gain slope vs. control voltage characteristic over a wide range of control voltages (see *Figure 2*), which greatly simplifies the implementation of AGC loop configurations.

Another kev advantage HMC992LP5E and the the HMC993LP5E their abilis ity to provide constant high OIP3 over the entire attenuation range. HMC992LP5E and HMC993LP5E differentiate themselves from traditional VGAs by providing constant

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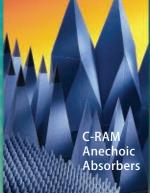
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OIP3 at any control voltage or attenuation level. *Figures 3A* and *3B* show that a constant OIP3 of greater than +40 dBm is achieved over the entire gain range.

The integrated power detector of the HMC992LP5E and HMC993LP5E exhibits excellent temperature stability. Both devices provide very accurate AGC closed loop power control, which is independent of part-to-part and temperature variations.

In open loop operation, VGA operation is achieved with two attenuators and two amplifiers by applying different gain voltages to the VCTRL pin. This pin is common to both attenuators in the VGA core, and operates between 1 and 4 V. Increasing the VCTRL pin voltage reduces the gain of the HMC992LP5E and HMC993LP5E VGAs and increases the input power level required for power saturation. These AGCs are well suited for transceiver applications

that require a single gain or power calibration setting during the manufacturing process.

In closed loop operation, the control voltage of the attenuator is driven by the RF detector, and the output power is automatically adjusted for a given VSET value. In other words, the output power is controlled by the VSET pin (see Figure 4). In such configurations, Hittite AGCs automatically compensate for the variations over temperature and part-to-part through the high accuracy power detector, to achieve repeatable linear power adjustments. Both the HMC992LP5E and the HMC993LP5E are designed to be used in closed loop operation, require only DC blocking capacitors and resistors, and are specified for operation from  $-40^{\circ}$  to  $+85^{\circ}$ C.

Figure 5 shows the output power vs. input power transfer characteristics of the HMC992LP5E over dif-

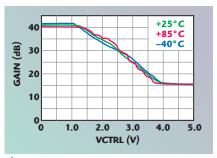
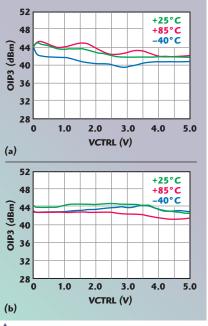


Fig. 2 HMC992LP5E gain vs. VCTRL at 100 MHz.



▲ Fig. 3 HMC992LP5E OIP3 vs. VCTRL at 300 MHz (a) and HMC993LP5E OIP3 vs. VCTRL at 900 MHz (b).

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ferent temperatures for a closed AGC loop configuration when VSET is 0.6 V. The figure shows that the device exhibits over 45 dB of dynamic range with a minimal output power variation of less than 1 dB over temperature.

Hittite Microwave's design philosophy involves choosing the best semiconductor processes and design techniques available to provide customers with market-leading solutions. This allows the system's designer to maximize the true potential of the

design and ultimately deliver a superior product. In most microwave radio and BTS receiver system configurations, the HMC992LP5E and the HMC993LP5E can be used to provide a space saving, single chip solution for each AGC block, while eliminating more than 18 discrete circuit elements. Moreover, these AGC devices can be combined with a number of additional catalog components from Hittite to implement high performance, end-to-end communication solutions.

### 

▲ Fig. 4 HMC992LP5E output power vs. VSET over input power at 300 MHz (closed loop configuration).

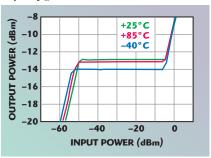


Fig. 5 HMC992LP5E output power vs. input power at 400 MHz and VSET = 0.6 V.

The HMC992LP5E and the HMC993LP5E provide complete, high value and highly accurate IF and RF power control solutions for a wide range of communications applications. Designed to be used in both open and closed loop operation, they both offer excellent linearity, a wide gain control range and configuration options with one or two attenuators depending upon the dynamic range requirements of the application. Compared with discrete implementations, the HMC992LP5E and the HMC993LP5E deliver a simpler, more flexible and compact design that reduces PCB space and features excellent temperature stability which is independent of part-to-part variations. The HMC992LP5E and HMC993LP5E can be combined with a number of different Hittite high performance catalog components to implement a wide range of market solutions for LTE/WiMAX/4G, microwave radio, VSAT, test equipment and sensor applications.

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746 ~ 780				*	*	
860 ~ 894			*	*		*
925 ~ 960	*			*		*
1525 ~ 1559				*		
1805 ~ 1880				*		*
1930 ~ 1980	*			*		*
2110 ~ 2170	*	*		*		
2300 ~ 2400	*					*
2469 ~ 2690				*		*
2570 ~ 2690	*	*		*		

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Part Number	Frequency (MHz)	Pout (W)	ACLR without DPD (dBr)	Efficiency (%)	Power Gain (dB)	Dimension (mm)
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RTH08007-10	860 ~ 894	7.07	-30	40	17	28 x 19 x 6
RTH09007-10	925 ~ 960	7.07	-30	40	17	28 x 19 x 6
RTH15007-10	1475.9 ~ 1510.9	7.07	-30	40	16	28 x 19 x 6
RTH18007-10	1805 ~ 1880	7.07	-30	40	16	28 x 19 x 6
RTH21007-10	2110 ~ 2170	7.07	-30	40	15	28 x 19 x 6
RTH27007-10	2620 ~ 2690	7.07	-30	40	14	28 x 19 x 6

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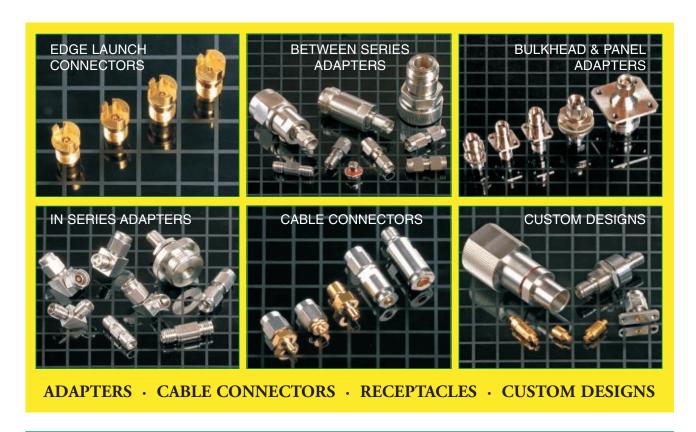
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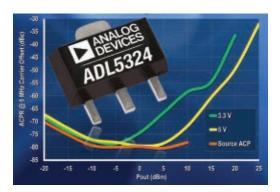
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# Half Watt Driver Amplifier with Dynamically Adjustable Bias

Today's radio designs, and other RF communication equipment, are being made to consume less power while occupying less physical space, which leads to less available board area for heat sinking. In addition, these systems are being deployed in more extreme environmental conditions where only passive cooling is being used, which leads to the need for very reliable ICs that can withstand greater temperature variations. When the factor of system output power scalability gets added in, then the need emerges for a new equally scalable RF driver amplifier. To satisfy all of these goals, Analog Devices introduces the ADL5324 ½ W SOT-89 RF driver amplifier.

The ADL5324 incorporates a dynamically adjustable biasing circuit that allows for the customization of OIP3 and P1dB performance from 3.3 to 5 V, without the need for an external bias resistor. This feature gives the designer the ability to tailor driver amplifier performance to the specific needs of the design. The adjustable bias also allows for the driver to be dynamically biased in order to conserve power consumption when the full performance of the driver amplifier is not required, such as when a system is in stand-by mode. This scalability reduces the need to evaluate and inventory multiple driver amplifiers for different output power requirements, from 25 to 29 dBm output power levels. The ADL5324 is also rated to operate across the widest temperature range of

-40° to +105°C for reliable performance in designs that will experience higher temperatures, such as power amplifiers. The ½ W driver amplifier also covers the wide frequency range of 400 to 4000 MHz, and only requires a few external components to be tuned to a specific band within that wide range. This high performance broadband RF driver amplifier is well-suited for a variety of wired and wireless applications including cellular infrastructure, ISM band power amplifiers, defense equipment and instrumentation equipment.

The ADL5324 GaAs HBT ½ W driver amplifier consumes a low 5 V current of 133 mA and delivers best-in-class performance with an OIP3 of 43.1 dBm, a P1dB of 29.1 dBm, a gain of 14.6 dB and a low noise figure of 3.8 dB at 2140 MHz. When the bias voltage is reduced to 3.3 V the driver only consumes 62 mA and delivers an OIP3 of 34.4 dBm, a P1dB of 25.3 dBm, a gain of 13.6 dB and a lower noise figure of 3.2 dB at 2140 MHz. The driver amplifier can also be biased anywhere from 3.3 to 5 V to meet system needs that are in between the performance stated at 3.3 or 5 V. This feature creates the opportunity for dynamic biasing of the driver amplifier where a variable supply is used to allow for full 5 V biasing under large signal conditions, and then reduced supply

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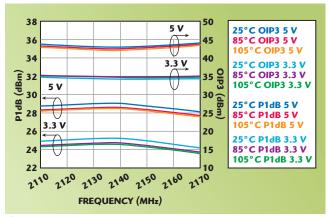


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### Product Feature



lacktriangle Fig. 1 ADL5324 OIP3 and P1dB vs.  $m V_{cc}$  and temperature showing that 3.3 to 5 V bias meets system needs.

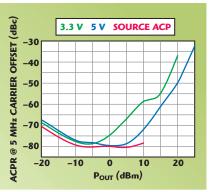


Fig. 2 ADL5324 ACPR vs. output power and V<sub>cc</sub> (3GPP 3.5 TM1-64 at 2.14 GHz) showing a minimal reduction to 15 dBm in the -55 dBc ACPR at 3.3 V bias

voltage when signal levels are smaller and lower power consumption is desirable (see *Figure 1*).

The ADL5324 also delivers excellent ACPR versus output power and bias voltage. The driver can deliver greater than 17 dBm of output power at 2140 MHz, while achieving an ACPR of -55 dBc at 5 V. If the bias is reduced to 3.3 V, the -55 dBc ACPR output power only minimally reduces to 15 dBm (see **Figure 2**).

The ADL5324 further simplifies RF design by eliminating the need for complicated external tuning. The driver only uses 50  $\Omega$  lines at the input and output of the amplifier and does not require a bias resistor. The ADL5324 only needs one shunt capacitor at its input and one shunt capacitor at its output for frequency tuning. The usual AC coupling capacitors and DC bias choke inductor are also required, along with the standard bypass capacitance on the DC bias trace.

The ADL5324 was also designed and packaged to simplify thermal considerations. The driver has best-

current consumption of 133 mA with 5 V, which reduces the amount of heat that is created. The 3.3 V current consumption is reduced to 62 mA. which further reduces the amount of heat created. The standard SOT-89 package also has large backside ground paddle that allows for an efficient thermal trans-

fer path from the driver amplifier. The data sheet shows the recommended circuit board land pattern with added thermal transfer vias to further improve thermal transfer from the driver amplifier. This allows the driver to be kept within safe operating temperatures without the need for forced air cooling, and the driver is fully specified over the widest operating temperature range of  $-40^{\circ}$  to  $+105^{\circ}$ C. The driver amplifier is also rated to an ESD rating of  $\pm 3$  kV (HBM, Class 2), which makes it equally robust in high volume manufacturing environments.

Another way Analog Devices helps improve RF design is with the amount of information provided in the ADL5324 data sheet. Data provided such as critical parameter variation versus temperature, from -40° to +105°C, voltage supply, from 3.3 to 5 V, and operating frequency, from 400 to 4000 MHz, reduces the amount of qualification time a designer needs to spend. That reduction in qualification time can significantly improve a projects' time-to-market. The comprehensive data sheet also allows the designer to accurately determine the least amount of power consumption achievable to meet the performance goals for their given application.

Analog Devices improves RF design in multiple ways; through innovative circuit design, simplified tuning requirements and detailed data sheet information. These attributes allow RF designers to go to market quickly with solutions that meet their needs for smaller, lower power consuming systems.

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Product scale 1:3



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# Exploit the Radio Channel for Improved MIMO Performance



Janne Kolu, Vice President of Test Tools,
EB (Elektrobit), explains the company's global reach, elaborates on the evolution of test systems in the wireless sector and discusses EB's latest product developments.

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high-quality services with higher data rates, requiring new wireless technology innovations that are able to meet the increased demand for high data rate applications. Physical layer performance improvements are being implemented, e.g. LTE technology is based on wider bandwidths, adaptive multi-antenna technologies – multiple-input, multiple-output (MIMO) – and in further 3GPP LTE-Advanced technology, enhanced transmission schemes like carrier aggregation and coordinated multipoint (CoMP).

Physical layer performance depends strongly on radio channel characteristics, especially in MIMO technologies, since MIMO offers significant performance gain in data throughput,

quality of service (QoS) and cell coverage without additional bandwidth or signal transmit power. Hence, MIMO technologies, such as spatial multiplexing (SM), beamforming (BF) and spatial diversity are setting challenging requirements for radio channel modeling and emulation capability in testing wireless communication networks and devices. At the same time as the technology evolution, time to market expectations are rising despite the more complex technology, requiring more effective design and verification methods and calling for more capacity, accuracy and effectiveness compared to past development methods.

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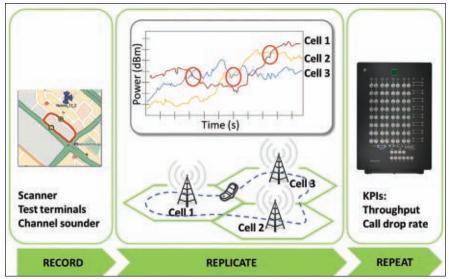
Therefore, EB (Elektrobit) has introduced a new EB Propsim® F32 radio channel emulator product to meet the demanding design and verification challenges of today's and future wireless technologies. It is designed for testing complex MIMO scenarios as well as enhanced transmission schemes. In addition, all these different test scenarios can be carried out either traditionally as conductive test via coaxial cable connections or Over-the-Air (OTA) together with the EB MIMO OTA application.

### **MIMO TESTING**

EB Propsim F32 emulates the typical radio channel characteristics like path loss, multipath fading, delay spread, Doppler spread, polarization and spatial parameters such as Angle of Arrival (AoA) and Angular Spreads (AS), which

are critical for MIMO system performance. It is designed for LTE testing supporting carrier bandwidth up to 40 MHz and frequency bands up to 2700 MHz, and features a compact and highly integrated design.

The new channel emulator is also scalable and allows the tailoring of the product configuration to current needs and the upgrading of features as technologies evolve. EB Propsim F32 can emulate up to 128 independent fading



tial parameters such as Angle of Arrival  $\triangle$  Fig. 1 Virtual drive testing with EB Propsim F32 enables MIMO handover scenarios incor-(AoA) and Angular Spreads (AS), which porating three or more simultaneous base stations in a single lab instrumentation.

channels simultaneously representing bi-directional  $8\times8$  MIMO emulation capability needed, e.g. in multi-user MIMO testing.

Now, typical TD-LTE beamforming or advanced MIMO OTA test systems can be equipped with a single radio channel emulator, making test setup and configuration cost effective, quick and easy, without the need for external hardware components and complicated synchro-





# Learn From the Experts About GaN Business Opportunities

**Special Panel Session at IMS 2012** 

### Where are the Emerging RF Market Opportunities for GaN?

Wednesday, June 20 8:00-10:00 AM Room 516

### Palais des Congrès de Montréal

Industry experts from Strategy Analytics, RFMD, TriQuint, Cree, NXP, Nitronex and UMS will make brief presentations about their view on GaN market opportunities followed by a question and answer session with the audience. This event is open to all attendees and complimentary breakfast will be served.



### **Product Feature**

nization of multiple instruments in the test system. High emulation capacity and high channel fidelity combined with excellent RF performance simplifies the test system installation and configuration for multi-antenna and multi-radio testing.

### **INTELLIGENCE BUILT-IN**

EB Propsim F32 has intelligent internal signal summing and splitting designed for testing of different link topologies with user-defined antenna connections to the instrument. Flexibility in physical antenna connections, integrated local oscillators and signal duplexers together provide convenient and reliable test system installation with good support for remote use and 24/7 test automation, even for multi-RAT testing.

It is equipped with the standard Windows XP embedded operating system that is familiar to any user and therefore the emulator is easy to configure for remote desktop use when the laboratory facility and office desk are in different locations. The radio channel emulator ensures low operating costs by fast test system configuration and convenience of channel modeling capabilities.

### **VIRTUAL DRIVE TESTING**

The EB Propsim F32 makes it easy to improve test effectiveness by creating realistic Virtual Drive Testing (VDT) (see  $Figure\ 1$ ) or network level test scenarios including multiple base stations and user terminals in repeatable lab conditions. Traditional field-testing of wireless systems is labor intensive, time-consuming and expensive. Also, getting consistent results is a challenge. EB's VDT application together with the high capacity EB Propsim F32 solves these problems by enabling VDT in laboratory conditions.

VDT utilizes the field measurement data from real live networks captured by drive test tools or channel sounders in order to create repeatable real-world like conditions to laboratory testing. All the elements of the real environment: fast fading, Doppler, signal level variations, interference and antenna parameter effects can be replicated, making it possible to isolate performance issues early in the development and design verification phase.

Being compatible with various drive test tools, EB VDT with the new EB Propsim F32 is a powerful solution for operators, network, device and chipset manufacturers by verifying the performance and interoperability under different realistic field conditions. The new radio channel emulator allows simultaneous connection, e.g. three base stations and five terminals or five groups of terminals for bi-directional LTE 2×2 MIMO testing. This setup enables true performance testing, including different handover scenarios, scheduling, power control, etc., under dynamic and realistic propagation conditions.

### **MIMO OTA TESTING**

EB MIMO OTA application expands the usage of the EB Propsim F32 from traditional conductive testing to MIMO OTA testing. MIMO OTA testing is a state-of-theart test method for mobile device, chipset and antenna designers and manufacturers working on MIMO technologies. MIMO OTA testing with the new radio channel







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### **Product Feature**

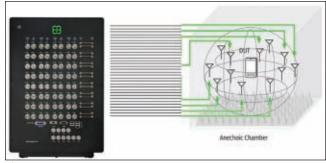


Fig. 2 The EB Propsim® F32's compact design also allows a higher number of probes in the MIMO OTA chamber.

emulator enables the evaluation of the end user experience of the final product, e.g., in terms of data throughput, against realistic radio channel conditions where performance varies greatly according to environment.

The unit's compact design also allows a higher number of probes in the MIMO OTA chamber (see *Figure 2*), thus radiated multipath signals generate more accurate radio channel environment around the DUT. EB Propsim F32 in MIMO OTA testing enables the real-world performance evaluation by providing the answer to the question, "How good is my terminal?"

### **ACCELERATED DEVELOPMENT CYCLES**

Realistic field scenarios in laboratory testing at the early development stages provide immediate feedback and facilitate the improvement of product maturity before field trials, thus accelerating the product development cycles and yielding better product quality. EB Propsim F32 provides high capacity and convenience for testing demanding broadband multi-antenna wireless devices as well as complex and realistic network level test scenarios in laboratory conditions. Testing with the new radio channel emulator provides good network performance, high quality user experience of devices and hastens the time to market of new wireless devices and systems.

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# Wideband Synthesized Signal Generators

ini-Circuits has developed two new wideband synthesized signal generators. The SSG-4000HP is a wideband synthesized signal generator that operates over the frequency range of 250 to 4000 MHz providing a 70 dB power range from -50 to +20 dBm in 0.25dB steps and the SSG-4000LH (both RoHS compliant) operates over the same frequency range providing a 70 dB power range from -60 to +10 dBm in 0.25 dB steps. They can be set to sweep either power or frequency up, down or bi-directionally (sawtooth). The SSG-4000HP is encased in a rugged metal shielded

package of  $8.37" \times 8.5" \times 2.15"$  while the SSG-4000LH is packaged in a case of 11"  $\times$  8.5"  $\times$  2.15". Both are equipped with an N-type 50  $\Omega$  connector at the RF output port. They are powered by a supplied three wire 24 V AC/DC power adapter (grounded) and controlled through a USB 2.0 interface using a unique user friendly GUI software allowing the user to select one of several different output modes including both frequency sweep and power sweep (up, down or bidirectional) options.

Both wideband synthesized signal generators are plug-and-play (no need to install a driver for the device)

and supplied with a CD containing programming instructions for Linux® and Windows® operating systems (32 and 64 bit systems) and a Windows® GUI control program containing an API DLL com object is included. Also included are a 2.7 ft USB cable and a power adapter suitable for U.S., EU and other power systems. Longer USB cables and a mounting bracket are available as additional options.

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# Small Vector Reflectometer

opper Mountain Technologies has developed a new class of vector network analyzer, the virtual vector reflectometer PLANAR R54, operating in the frequency range of 85 MHz to 5.4 GHz (specified to 4.2 GHz). The device functions with a virtual UI and is powered and operated via a single USB interface on any external Windows PC.

PLANAR R54 implements many of the functions of advanced vector reflectometers, measuring various characteristics of the  $S_{11}$  parameter: return loss, VSWR, phase, impedance (Smith chart), etc. It also operates in time domain measuring DTF with high accuracy. With a frequency setting

resolution of 10 Hz and up to 10,001 measurement points per sweep, R54 performs on par with industry leaders, but at a fraction of the cost.

The device has a uniquely compact form factor:  $117 \times 39 \times 19$  mm and weighs only 8.8 ounces, using less than 2 W for power. These dimensions are no accident – the device is as small as the minimum bend radius of a test cable which allows for direct connection to any DUT where a test cable could be connected. The ability to easily connect to a DUT without the use of a test cable improves the accuracy of testing, decreases cost and allows for more efficient and less frequent calibration.

The combination of advanced features, high accuracy and value of the PLANAR R54 makes this vector reflectometer well suited for daily use by specialists in the field as well as in the lab and production environment. The software interface of the R54 is compatible with the latest in notebook and tablet technology (including touch screens), allowing for the portability in the field.

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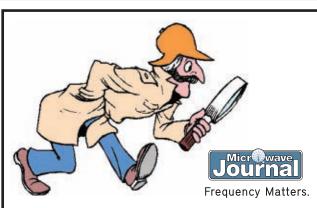
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### **IMS 2012 Products Scavenger Hunt**

An IMS exhibition attendee has a lot of vendors to visit in a short period of time. To find what you need, you need to know where to look. Take the challenge and complete this month's Scavenger Hunt on pg. 282.

Drop off the completed puzzler to MWJ Booth #2018 and be entered into a daily prize drawing for a Kindle Fire.

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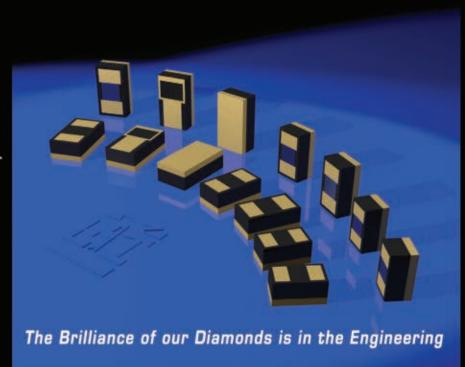
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### HIGH POWER HIGH FREQUENCY CVD DIAMOND CHIP RESISTORS

The RPCO402DR series of resistors offers excellent power handling capabilities and frequency response to 30GHz. The superior thermal properties of CVD diamond (high conductivity and low expansion) makes these resistors ideal for pulsed power applications. The mechanical and electrical characteristics of these chips provide a robust solution for many aerospace and militaryapplications while its standardized production process keeps the cost competitive for commercial use.



### Specifications:

Resistance: 50 and 100 0hms, +/-5%

Frequency: DC – 30 GHz

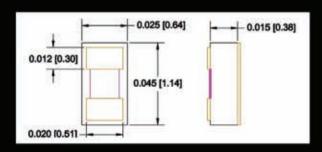
Power: 20 Watts

Capacitance: O.1 pF Max

• Operating temperature: -55 °C to 150 °C

CVD diamond substrate

Solderable or wire bondable terminals





### Features:

- · High frequency response DC-30GHz
- · High power, 20W CW in 0402 size
- 5x power dissipation than equivalent size BeO components
- Ultra small, compact design
- Low capacitance < 0.1 pF</li>
- Total thin film constriction
- Surface mount or flanged (integrated heat sink)
- Excellent pulse power handling
- RoHS compliant
- Hi Rel version available

### Applications:

- Satellite communications
- Phased array radar
- Telemetry
- Test and measurements
- · High power amplifiers
- · Phase shifters

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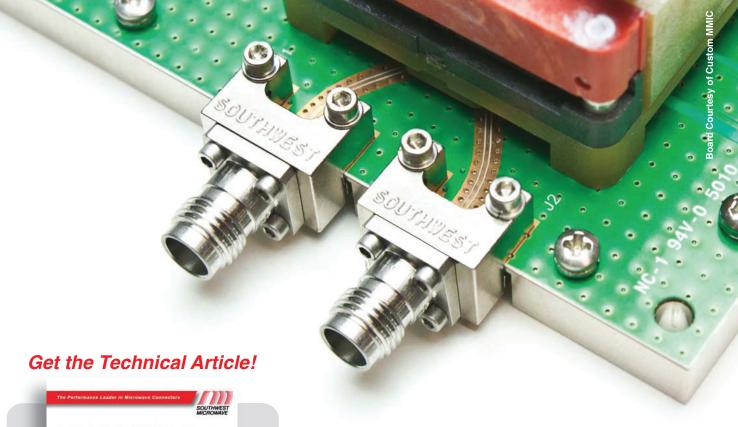
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TRS-RenTelco	332	5
TRU Corp		
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ITE Inc	. 30	0
ITM Technologies Inc	350	0
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UltraSource Inc	200	o
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UMS (United Monolithic		
Semiconductors)	161	c
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UTE Microwave Inc	232	1
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Vacuum Engineering & Materials Co. Inc		
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VidaRF	152	1
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Viper RF Ltd	352	5
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Virginia Diodes Inc	122	8
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Voltronics Corp./Dover	141	U
VTI Instruments Corp	. 91	5
W. L. Gore & Associates Inc	232	4
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Wenzel Associates Inc	311	2
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West Bond Inc	190	1
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WIN Semiconductors Corp	281	6
WIPL-D D.O.O	62	3
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X5 Systems Inc	. 62	2
Xi'an Forstar S&T Co. Ltd		
Xi'an Gold Waves S&T Co. Ltd	310	7
Yantel Corp	340	7
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Yokowo Co. Ltd	. 11	1
Yortec Inc	. 20	2
Z-Communications Inc		
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- Instrumentation:
  - -Test and Measurement

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# IMS PRODUCT SHOWCASE IMS SHOW FLOOR



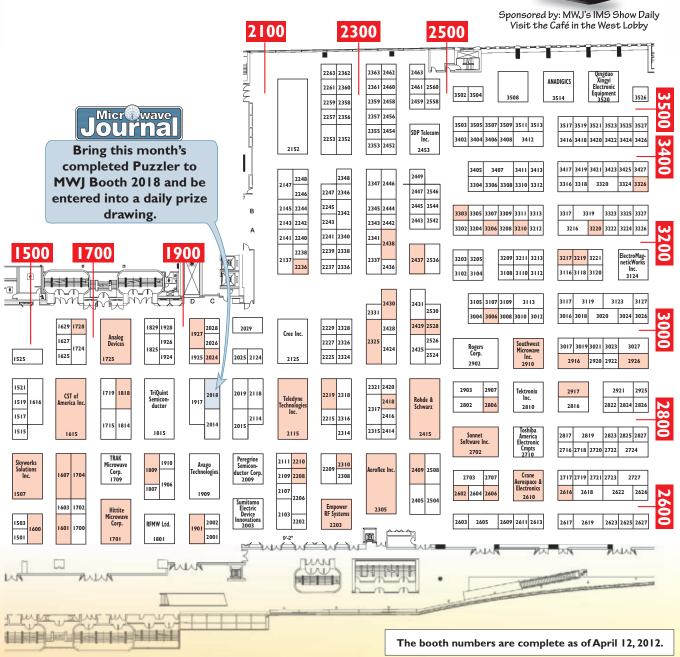
# Your Product Guide to the Show Floor

Shaded exhibitors have a product featured in the IMS Product Showcase pages to follow. Look for these products at this year's IMS 2012.

**MicroApps Expert Forum** 

**Device Characterization and Design** Wed. at 12:00 PM, June 20th 20D M 129 228 629 728 729 828 829 928 929 1030 1029 1128 1129 1228 727 826 127 226 1127 1226 627 726 MITEQ Inc. MicroApp 125 224 425 524 925 1024 1125 1224 525 624 123 222 423 522 1123 1222 121 220 321 420 419 518 119 218 319 418 Maury Microwave Corp. National 917 1016 117 216 115 214 K&L 1410 NXP conductors Anritsu Co. ANSYS Inc. 105 204 1305 1404 1201 1300 101 200 国十年



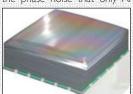


### IMS PRODUCT SHOWCASE AISLES 100-500

The following booth numbers are complete as of April 12, 2012.

### APA Wireless Booth 112 4200 to 4600 MHz of Bandwidth

Running 128QAM and starving for bits? You need the phase noise that only APA's Physics Based



Technology can provide. Fundamental mode operation, 400 MHz of continuous bandwidth, bestin-class phase noise within the

4 to 5 GHz band and linear tuning that won't wreck your loop dynamics. Fully characterized over the industrial temperature range, phase hit free and 100 percent factory tested ensures every bit you send is "in the clear."

www.apawireless.com

### **Laser Services**

Booth 215

### Circuit and Material Laser Cutting



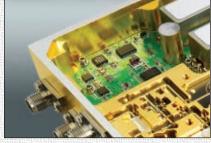
Stop by booth #215 to learn about Laser Services and its one-stop job shop that includes laser cutting of your EMI and bonding materials and solder damming in circuits using laser ablation. The company also has an extensive inventory of ceramic substrate, frozen epoxies, and adhesives that can be custom cut or drilled for just-in-time delivery.

VENDOR**VIEW**www.laserservicesusa.com

### SemiGen

Booth 301

### RF Assembly Services and Supply Center



Stop by booth #301 to learn about SemiGen and its RF/microwave hybrid assembly and testing, automated PCB manufacturing capabilities and semiconductor diodes and capacitor products. The company recently opened an eCommerce R Supply Center, which is fully stocked with some of the most popular bonding supplies, adhesives and epoxies ready for just-in-time delivery.

www.semigen.net

### Anoison Electronics Booth 310

**Coaxial Terminations** 



Anoison Electronics announces that it has expanded its product offering to include a full line of RF coaxial terminations. In addition to standard SMAs, 7/16, QMAs, SMPs, and Ns in both male and female configurations, it also offers high performance QNs (HPQN), high performance TNCs (TNCA), and 2.92s (SMK). Male SMAs and Ns are also available as Push-Ons.

www.anoison.com

### Copper Mountain Technologies

Booth 317

### Virtual Vector Reflectometer



Copper Mountain Technologies introduces a new class of vector network analyzer, the virtual vector reflectometer PLANAR R54, operating in frequencies from 85 MHz to 5.4 GHz. Portable and lightweight, R54 is powered and operated via a single USB interface by external PC. Comparable to industry leaders, but at a fraction of the cost, R54 is ideal for use on DUTs in the field accurately and without the use of testing cables.

WENDOR**VIEW**www.coppermountaintech.com

### Planar Monolithics Industries Booth 403

**Log Video Amplifier** 



PMI model SDLVA-8G18G-40-5-SFF is an 8 to 18 GHz successive detection log video amplifier that is supplied in a ruggedized, hermetically sealed housing that measures only 1.2" L  $\times$  0.85" W  $\times$  0.4" H.This model operates on a single +5 V DC supply and consumes less than 130 mA of current. It is highly temperature compensated such that the log linearity is better than  $\pm 1$  dB over the temperature range of -54° to +85°C. This model has a logging range of -40 dBm to 0 dBm with an output log video voltage of 10 mV to 2.25 V. This model features a fast rise/fall time of 25 ns/30 ns and a recovery time of less than 40 ns.

WENDOR**VIEW**www.pmi-rf.com

### Renaissance Electronics

Booth 500

### **Ultra High Power Circulator**



Renaissance's latest ultra high power circulator is designed for VHF, cellular and military commu-

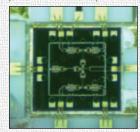
nication applications and is robust enough to handle harsh environments. Learn more about it here: www.rec-usa.com/Data%20Sheets/ultrahigh-powercircusm.pdf.

**VENDORVIEW** 

www.rec-usa.com, www.hxi.com.

### IKE Micro Booth 50 I Build to Print Manufacturing

For over 30 years, IKE Micro has been providing precision build to print manufacturing of RF/



microwave packages and modules. Latest model automated die attach, wire/ribbon wedge bonding, ball bonding, and top notch manual assemblers insure repeatable re-

sults. IKE targets mid to large sized production runs, serving the defense and commercial markets. ISO Certified and ITAR Registered.

www.ikemicro.com

### Bonding Source Booth 503 Epoxy Pre-Forms



Bonding Source offers quick delivery epoxy pre-forms to its defense and commercial customers and has complete storage and handling con-

trol with its in-house laser cutting capability. Bonding Source also stocks epoxy pastes and film, bonding wire and tools and accessories. Bonding Source has served over 500 customers worldwide.

www.bondingsource.com

### JQL Electronics Booth 508 Circulator and Isolator



JQL Electronics Inc. introduced a new series of drop-in circulator and isolator with ultra low intermodulation performance at -90 dBc max, designed for LTE. The new model series of drop-in circulator and

isolator covers all 25 LTE bands with typical insertion loss of 0.18 dB, isolation and return loss of 23 dB.

www.jqlelectronics.com

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300 MHz to 12 GHz



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- Low Profile, only 0.06"/1.5 mm thick

Mini-Circuits new MAC mixer family combines rugged ceramic construction with monolithic quad semiconductor technology to produce the most reliable mixers available in the marketplace today—the only mixers anywhere backed by a 3-year guarantee! Top to bottom, inside and out, they're designed and built for long-term reliability under hostile conditions such as high moisture, vibration, acceleration, and thermal shock from -55 to +125°C.

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**Excellent electrical performance** across the entire frequency range makes them ideal not only for aerospace and military ground applications, but anywhere long-term reliability adds bottom-line value: instrumentation, heavy industry, high-speed production, and unmanned facilities, to name just a few. So why wait? Go to minicircuits.com for performance data, technical specifications, and remarkably low prices, and see what MAC mixers can do for your applications today!

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# IMS PRODUCT SHOWCASE AISLES 500-700

IW Microwave Booth 509

**Cables and Assemblies** 



W's Re-Flex™ cables have been tested to more than 24,000 bends with no electrical or mechanical degradation. These cables were designed to offer an alternative to standard semi-rigid and conformable cables. They have the same leakage characteristics and mechanical dimensions as standard semi-rigid cable. Stock assemblies use SMA plugs. Other connector styles are available. Standard cable diameters are RF 047™, 085™, 141™ and 250™. An FEP jacket is also provided upon request.

www.iw-microwave.com

### RLC Electronics Booth 510

### **Waveguide Switches**

RLC Electronics' electromechanical waveguide switches offer a compact design utilizing a proprietary non-contacting actuator mechanism that requires low current. These units are available in SPDT and transfer configurations, manual or re-



mote, with a choice of coil voltages and optional indicator contacts. Solid state de-energizing circuiting insures high reliability available with common positive. common negative and TTL control options.

A precision machined waveguide transition assembly is combined with coaxial switch technology to produce a device that features the low current and fast switching time of a coaxial switch with waveguide inputs and outputs.

www.rlcelectronics.com

### Times Microwave Booth 514

Coaxial Cables



PhaseTrack® coaxial cables are now available in standard flexible, low smoke flexible, in-the-box flex and semi-rigid versions. Exhibiting superior phase performance with temperature changes, they eliminate the common "phase knee" found in PTFE-based cables. Systems requiring phase stable or phase tracking interconnects will benefit from the performance offered by the Times PhaseTrack products, which offer superior absolute phase

performance, with tracking better than 50 ppm, and low insertion loss and VSWR characteristics.

www.timesmicro.com

### Emerson Connectivity Solutions Booth 60 I

**QPL Attenuators** 



Emerson Connectivity Solutions' Midwest Microwave product line of Qualified Parts List (QPL) attenuators are qualified, manufactured and tested to the strict requirements of

the MIL-DTL-M3933 product specification. The company's QPL line of M3933/14,/16,/17 and /25 SMA and TNC attenuators are ruggedly constructed to meet performance needs in the harshest of military environments. To service your delivery needs, Emerson strives to make most dB values available in short lead times or even off the shelf, for the most common values.

www.emersonconnectivity.com

### Mercury Computer Systems Booth 618

**Echotek Series Tuner** 



The Echotek Series RFM-251-XMC tuner from Mercury is engineered for applications that require RF tuning and data conversion flexibility within a compact slot-saving package. Tuning over a broad frequency range and then converting to digital IF, this XMC delivers the functionality required for applications that must operate under SWaP-constrained platforms. The RFM-251-XMC tuner supports a broad frequency range from 20 to 2500 MHz. This coverage is ideal for intercepting frequencies associated with a wide range of communication bands.

www.mc.com



### Anaren Booth 709

### **Surface-Mount Delay Lines**

Anaren's new surface-mount delay lines use a slow wave coupling structure that maximizes the amount of delay per unit area over other distributed delay structures. These delay lines can be



used in amplifier linearization applications or in the main loop of feed forward and pre-distortion amplifiers. They are low cost.

high quality alternatives to the traditional coaxial and filter solutions presently available. Moreover, parts have been subjected to rigorous qualification testing and units are 100 percent tested. Available in RoHS-compliant finishes.

### **APECS Ceramic Solution**



Anaren Precision Etched Ceramic Substrates (APECS) from Anaren Ceramics Inc. can be combined with standard thick film technology to create a highly integrated, more cost-effective solution while improving overall substrate yield. The process also allows for integrate components, as APECS substrates accept embedded precision resistors, Lange couplers and capacitors into the substrate itself, rather than applying discrete components using the more labor-intensive, less-consistent traditional component-mounting approach.

www.anaren.com

### Carlisle Interconnect Technologies Booth 715

### **Push-On Connector Lines**

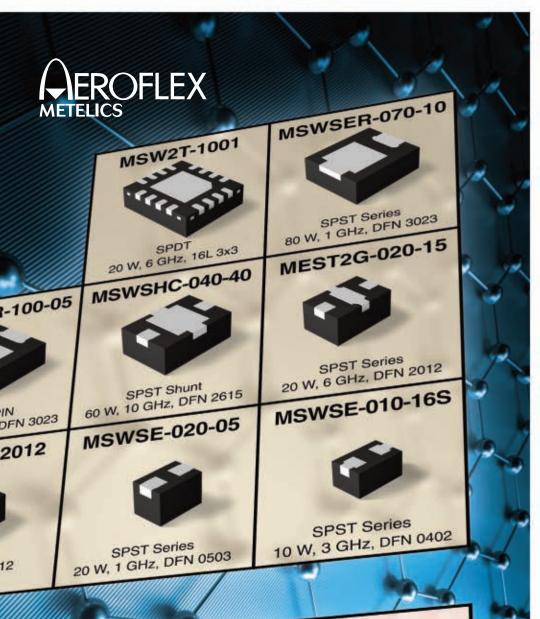


CarlisleIT has added two new connector lines to its push-on family - the TMP® and WMP® series.

The TMP family was designed to provide higher power handling capacity for Radar applications, while the WMP line provides the smallest form factor for space restricted applications. Both connector series provide the benefits of a push-on interface – i.e., simple connection and ease of use in dense package configurations – and include PCB mount, field replaceable, microwave cable, and custom connectors.

www.carlisleit.com

# Engineer the ideal switch from a brand new table of elements



Aeroflex / Metelics has created a suite of versatile control elements designed to move your next switch to another level of efficiency. The core component of the group is an integrated SPDT switch in a 3x3 mm QFN package. MSW2T-1001 gives you 0.3 dB of insertion loss and 24 dB of isolation up to 6 GHz. Five other SPST components offer a broad range of high power, low inductance, low capacitance choices that also deliver through 6 GHz, while 2 complimentary Schottky's give you detection solutions you can push to 18 GHz. They're all efficiently priced for high volume commercial applications.

Make the switch with Aeroflex / Metelics.

408-328-3321 www.aeroflex.com/metelics See us at IMS Booth 2305







### IMS PRODUCT SHOWCASE AISLES 700-1000

### Delta Microwave Booth 722 TCDL Diplexer



The model Ku5939 Ku-Band TCDL Diplexer has passbands from 14.4 to 14.83 GHz and 15.15 to 15.35 GHz with

less than 1.6 dB insertion loss in each of the channels in a compact 3.8"  $\times$  2.75"  $\times$  0.5" package. The unit shown has SMP Male connectors but is also available with SMA Female connectors under model number Ku5937. The maximum VSWR is 1.5:1 and the minimum channel-to-channel isolation is 110 dB. Either channel can handle +40 dBm at 40,000 feet.

www.deltamicrowave.com

### Pivotone Communication Technologies Booth 726

**Passive Components** 



Pivotone designs and manufactures RF and microwave passive components up to 50 GHz in frequency. The company operates

from an ISO9001:2008 facility in an ISO14000 business park in Wuxi, China – about 100 km from Shanghai center. A full range of products is offered including: filters, diplexers, combiners, hot standby couplers, loads, dielectric resonator filters, TMA for cellular applications and adapters, with passive and active involved (LNA monitoring communication card, etc. for the RF devices and modules).

www.pivotone.com

### Anritsu Co. Booth 807 Network Analysis System



Anritsu Co. will be showcasing its new VectorStar® Waveguide-Band Vector Network Analysis System. This follows-on

from the highly successful coaxial 70 kHz to 125 GHz Broadband Vector Analysis System. Available for E, and W-Band, it uses the same industry-leading nonlinear transmission line technology contained in the broadband system providing the same advantages of compact size, performance and stability. A wide range of applications is covered, including E-Band communications, automotive radar, imaging radars, on-wafer semiconductor measurements and materials research.

VENDOR**VIEW**www.anritsu.com

### M/A-COM Technology Solutions Booth 815

### **Smartset Chipset**



M/A-COM Technology Solutions will showcase its broad portfolio of products across 38 product lines. New product releases include

M/A-COMTech's 42 GHz Smartset Chipset for pointto-point wireless backhaul and GaN Smart Pallets for aerospace and defense radar applications. Also featured are a new set of standard catalog products including LNA, VGA, GPA and power detectors in ultra small packages for multimarket applications.

www.macomtech.com

### ANSYS Inc. Booth 907

### **Design Software**

ANSYS will demonstrate new features in HFSS™, the industry standard software for RF and microwave design. Learn how HFSS can solve your largest electromagnetic field simulations using advanced simulation techniques including domain decomposition, hybrid finite element/boundary integral, physical optics and high-performance computing. See the new HFSS ECAD option that allows you to operate HFSS from the ANSYS DesignerRF layout or from within the Cadence® software tools. These new advanced features deliver a comprehensive Simulation Driven Product Development environment.

www.ansys.com

### TRU Corp.

### Booth 924

### **Cable Assemblies**



TRU Corp. introduces a new standard in high performance, enhanced durability cable assemblies. TRU-core™ 300 offers superior resistance to crushing kinking and twisting of the cable without the need for any additional external armoring. This saves weight and cost while enhancing flexibility. The unique expanded PTFE core of the cable provides excellent phase and thermal stability. The assemblies are available with stainless steel SMA, Type N and ATNC interfaces for broadband DC to 18 GHz performance.

www.trucorporation.com

### **Booth 1015**

### **Agilent Technologies**

### Signal Analyzers



The Agilent EXA X-Series now has extended frequency coverage to 44 GHz – and up to 325 GHz with external mixing – making it the most cost-effective millimeter-wave signal analyzers on the market. Their exceptional sensitivity, < -140 dBm/Hz across the V-Band with smart harmonic mixers, enables accurate measurement of spurs and harmonics. Along with their excellent phase noise of -106 dBc/Hz typical (10 kHz offset at 1 GHz), EXA Series analyzers can meet the tighter regulations and test requirements for millimeter-wave device design and performance in aerospace and defense and wireless communications. The model N9010A-E32 provides frequency coverage up to 32 GHz and the model N9010A-E44 up to 44 GHz.

### **Handheld RF Analyzers**



Agilent enhances the FieldFox handheld RF analyzer family by adding two new options, time domain analysis (Option 010) and a built-in channel power meter (Option 311). The built-in power measurement capability provides a simple and cost effective approach to power measurements without the need for a USB power sensor. Using time domain and gating, you can test devices such as transmission lines, fixtures and connectors to characterize device discontinuities and identify impedance variations. Both options can be added to new units or existing customers can purchase as a software upgrade.

### **PIM Test Solution**



Agilent Technologies introduces a new test solution for passive intermodulation (PIM) of passive components for wireless communication industries. The innovative solution with the E5072A ENA series network analyzer combines both PIM and S-parameter tests with a single connection of devices under test to achieve measurement capabilities that are flexible, fast and accurate. With high receiver sensitivity of the E5072A, the solution offers measurements of extremely low PIM products, with levels of -170 dBc or better:

www.agilent.com



You work in all kinds of conditions, so should your spectrum analyzer.



Scan the QR code or visit http://goo.gl/Rfbde to see a HSA N9344C demo guide video Worst-case scenario: You've got minutes to troubleshoot RF interference that has shut down communications on the ground, at dusk, in the desert.

Best-case scenario: You've got the only spectrum analyzer with benchtop performance in a lightweight MIL-PRF 28800F Class 2 compliant handheld—with secure erase to keep classified data classified.

That's thinking ahead. That's Agilent.

### **Handheld Spectrum Analyzers (HSA)**

Key Specs	N9344C	N9343C	N9342C
Frequency	1 MHz– 20 GHz	1 MHz– 13.6 GHz	100 kHz– 7 GHz
DANL	-155 dBm/Hz	-155 dBm/Hz	-164 dBm/Hz
Sweep time	< 0.9 s	< 0.7 s	< 0.4 s
Weight with battery	3.6 kg (7.9 lbs)	3.6 kg (7.9 lbs)	3.6 kg (7.9 lbs)

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See us at IMS Booth 1015



# IMS PRODUCT SHOWCASE AISLES 1100-1300

### Auriga Microwave

### Booth 1122

### **Component Test System**



Auriga's turn-key, fully-automated, component test system radically changes the dynamics of complex RF measurements. CTS-3, the company's third generation custom test system, is a fully-automated, component test system that

provides a single-connection, multiple measurement architecture used in both low-volume and high-volume manufacturing of high-frequency commercial and military modules and MMIC devices, such as transmit and receive modules (T/R), LMDS and MMDS, CPE, and base station testing.

www.aurigamicrowave.com

### OML Inc.

### Booth 1126

### **Harmonic Mixers**



OML offers harmonic mixers and standard gain horn antennas for testing compliance according to FCC Part 15 regulations on transmitters operating in the 10 to 100 GHz spectrum. Per FCC 15.33, four waveguide bands (WR-19, WR-12, WR-08 and WR-05) enable measurements of the highest fundamental up to the fifth harmonic (or to 200 GHz). Standard gain horn antennas (+24 dBi) also satisfy ANSI C63.4, C63.5 and C63.10. This solution is compatible with most high performance spectrum analyzers offering optional external mixer capabilities (e.g., Agilent PXA).

www.omlinc.com

### Vaunix

### Booth 1129

### **Lab Brick Test Equipment**



Stop by booth 1129 to check out Vaunix's Lab Brick family of low cost USB powered digital attenuators, LSG and LMS Signal Generators, and their latest LSW

Series Switch that offers reliable, high isolation and low cost solid state switching in both SPDT and SP4T configurations. Solutions up to 20 GHz are detailed at www.vaunix.com.

WENDOR**VIEW**www.vaunix.com

### AR RF/Microwave Instrumentation Booth | 20 |

### **Dual-Band Amplifiers**



With AR's dual-band amplifiers, you have freedom like never before. You pick the power from 5 to 80 W. You pick the bandwidth from 0.7 to 8 GHz, 0.7 to 10.6 GHz or 0.7 to 18 GHz. AR puts it together for you in one package that costs less, weighs less and takes less space than two separate amplifiers.

### VENDOR**VIEW**www.arworld.us

### **RFMD**

### Booth 1210

### Single FEM



The RFMD RFFM4501 provides a complete integrated solution in a single FEM for WiFi 802.11a/n/ac systems. Its small footprint and integrated matching minimizes the layout area in the cus-

tomer's application and reduces the number of external components. This translates to reduced BOM, footprint and manufacturing costs. The RFFM4501 integrates a PA, SPDT, LNA with bypass, and a power detector coupler for improved accuracy. It meets or exceeds the RF Front End needs of IEEE 802.11a/n/ac WiFi RF systems.

VENDOR**VIEW** 

### Virginia Diodes Inc.

### Booth 1228

### VNA Extension Modules



VDI's VNA extension modules provide high performance frequency extension of VNAs into the THz range. Models are currently available that cover 50 GHz to 1.1 THz and combine high testport power with superb dynamic range to offer unparalleled performance. For instance, at WR1.5 (500 to 750 GHz) typical dynamic range is 100 dB with -25 dBm test port power. The modules are compatible with all modern network analyzers. Contact VDI to discuss configurations that will yield the best performance for your application.

www.vadiodes.com

### Vectron

### Booth 1300

### **Ultra Low Noise OCXO**



The 10 MHz OX-204 is an ultra low noise OCXO achieving phase noise performance of -135 dBc/Hz at 10 Hz offset and -175 dBc/Hz at 100 KHz offset. The OX-204 has exceptional ADEV at 0.5 e-12 at 1 sec

tau and low long term stability of 100 ppb/year. The temperature stability is impressive at  $\pm 20$  ppb over the temperature range of -40° to +85°C. This is all achievable in a compact 25  $\times$  25 mm enclosure.

www.vectron.com

Let this month's Product Showcase help you fill-in the Scavenger Hunt questions on page 282.

### Maury Microwave Booth 1215

### **Measurement and Modeling Solutions**



Maury Microwave will be demonstrating state-of-theart measurement and modeling solutions including: a patent-pending noise parameter system, a pulsed IV/S-Parameter and compact modeling system, a hybrid-active harmonic loadpull solution based on the PNA-X, and a patented mixed-signal active loadpull system capable of up to 1000 impedance/power measurements per minute and 120 MHz of instantaneous impedance control. Maury's component division will

showcase its new Stability line of amplitude- and phase-stable cable assemblies as well as calibration kits, metrology and instrument-grade adapters and test essentials.

### Ruggedized Cable Assemblies

Maury Microwave's Stability™ series sets the standard for high-performance ruggedized cable assemblies. Designed specifically for phase-stable and amplitude-stable applications, Stability offers excellent measurement repeatability even after cable flexure. With a ruggedized, durable construction, Stability will outlast and outperform other assemblies resulting in a reduced total cost-of-test. Stability's light weight, superior flexibility and small form factor make it ideal for daily use with VNAs, test instruments, bench-top testing and ATE systems.

www.maurymw.com

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Sure, we sell lots of microwave and millimeter-wave components.

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# IMS PRODUCT SHOWCASE AISLES 1300-1600

### K&L Microwave Booth 1309 Narrowband Cavity Filter



From K&L Microwave's new CS series, this 3-section narrowband cavity filter has a center frequency of 1217.2 MHz with an equirpple bandwidth of 2.3 MHz minimum, yielding an insertion loss of 3 dB maximum.The out-of-band attenuation for this 3-pole filter is 52 dB minimum from DC to 1200 MHz and 46 dB minimum at 1230 MHz. VSWR is less than 1.5:1 over the passband. The size of this part is 5.7" × 5.3" × 3." SMA female connectors are shown, with other standard connector types available. The CS series of filters is excellent for narrowband applications where low insertion loss is required in the mid-band areas. Typical lead time is 5 to 6 weeks ARO.

www.klmicrowave.com

### National Instruments

### Booth 1315

### **Vector Signal Analyzer**



Engineers are looking for a faster, smaller, more cost-effective solution than classic rack-and-stack options. Compare the

speed and performance of NI PXI products to traditional boxed instruments. Experience the power of the NI PXIe-5665, I4 GHz RF vector signal analyzer in this video: www.ni.com/lp/comparepxi/?metc=mtjuaw.

www.ni.com

### MITEQ

### Booth 1425

### Low Noise Amplifier



The JDMW series of low noise amplifiers can cover the full 18 to 21 GHz Satellite Communications band. This series of LNAs are lightweight (less than 23 grams) and are hermetic making them an easy choice for extreme environments. The small size (1.18" × 0.87" square) and low power dissipation of less than a watt (12 V DC at 75 mA) make for versatile mounting locations in any

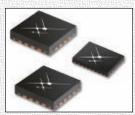
application. This unit has a noise temperature of 97 K (1.25 dB NF) and 30 dB of gain at  $\pm 25^{\circ}$ C. The full operating temperature range is  $\pm 30^{\circ}$  to  $\pm 65^{\circ}$ C with a power output (at 1 dB) of  $\pm 8^{\circ}$ 8 dBm. Optional RF input limiters, DC power connections and waveguide flanges are also available.

### WWW.miteq.com

### Skyworks Solutions Inc. Booth 1507

### **SPDT Switches**

The 50 W SKY12207-478LF (0.9 to 4 GHz) and SKY12208-306LF (0.02 to 2.7 GHz), and the 100 W SKY12210-478LF (0.9 to 4 GHz) switches deliver low insertion loss, excellent power handling,



superb linearity with low DC power consumption and high antenna-to-receive isolation for T/R and failsafe switching in TDD-LTE, TD-SCDMA base stations, repeater

and low frequency military radios. They are available in small  $4 \times 4 \times 1.5$  mm, 16-pin QFN packages.

### WWW.skyworksinc.com

### Synergy Microwave Corp. Booth 1600, 1601

### **High Frequency Oscillator**

The HFSO 1000-5 is an ultra-low phase noise oscillator that can be phase locked for single frequency applications as reference frequency



translators for instrumentation and radar markets. These products are vital for carrier signal sources in radar and as clocks in high speed ADC in

DDS synthesizers. This voltage tuned oscillator offers significant noise floor improvement over multiplied crystal oscillator solutions employed today.

### **High Resolution Synthesizer**



band (400 to 1100 MHz) small surfacemount synthesizer model MTS2500-40110-10 delivers a powerful per-

This ultra wide

formance. This small 1.95"  $\times$  1.25" surface-mount synthesizer delivers step size resolution down to 1 Hz. A low "close-in" phase noise (-105 dBc/Hz at 1 KHz, -106 dBc/Hz at 10 KHz offset, and -115 dBc/Hz at 100 kHz), a powerful buffered output (+8 dBm minimum), and a fast settling time (< 6 msec. within 10 Hz).

www.synergymwave.com

### Herley General Microwave Booth 1607

### **Indirect Synthesizer**

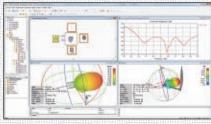


Herley General Microwave presents its model SF6218 — a state-of-the-art Fast Indirect Synthesizer designed to meet the high performance requirements of today's most demanding airborne, naval and ground electronic warfare systems. In addition, model SF6218 can also serve as a cost effective signal source for use in ATE and BIT applications. Its fast settling time, very low phase noise and wide frequency coverage are based upon a proprietary design utilizing high performance VCOs and DDS resulting in model SF6218 setting a new standard for performance-to-cost value.

www.herley.com

### Computer Simulation Technology Booth 1615

### **Project Management Software**



Version 2012 of CST STUDIO SUITE benefits from a new project management environment "System Assembly and Modeling" (SAM) which simplifies the management of simulation projects. SAM helps engineers to compare the results of different model configurations within one simulation project. A linked sequence of solver runs can also be initiated. All simulations and links can be defined in SAM to enable for example a seamless multiphysics work flow.

### WWW.cst.com



# WINDERAND.

### **Features**

- > Low Cost
- > Wide Bandwidth
- > Good Amplitude / Phase Unbalance
- > Rugged Welded Construction
- > RoHS Compliant
- > Patented REL-PRO Technology
- > 0.150" x 0.150" x 0.150"



Model Number	Frequency (MHz)	Impedance Ratio	Schematic
TM4-0	0.2 - 350	4:1	JE
TM1-0	0.3 - 1000	1:1	JE
TM1-1	0.4 - 500	1:1	JE
TM1.5-2	0.5 - 550	1.5:1	JE
TM2-1	1 - 600	2:1	JE
TM1-6	5 - 3000	1.1	0-ww-0
TM2-GT	5 - 1500	2:1	Ţ
TM4-GT	5 - 1000	4:1	Ţ
TM8-GT	5 - 1000	8:1	ŢŢ
TM4-1	10 - 1000	1:4	
TM4-4	10 - 2500	1:4	# (m)
TM1-2	20 - 1200	13	JE.
TM1-9	100 - 5000	1:1	0_vvv0 0=vvv0
TM1-8	800 - 4000	1.1	مسسوه



For additional information, contact Synergy's sales and application team.

Phone: (973) 881-8800 Fax: (973) 881-8361 E-mail: sales@synergymwave.com

# IMS PRODUCT SHOWCASE AISLES 1700-1800

### Hittite Microwave Corp. Booth 1701

**PLL with Integrated VCO** 



PLLs with Integrated VCOs are used throughout modern high performance communication systems. Hittite recently released a new 25 to 6000 MHz HMC833LP6GE PLL with integrated VCO for use as an LO in a transceiver. This device has a maximum phase detector frequency of 100 MHz in fractional mode and 125 MHz in integer mode. Floor figure of merit (FOM) is -227 dBc/Hz in fractional mode and -230 dBc/Hz in integer mode. At 2 GHz, its LO achieves -114 dBc/Hz at 10 kHz offset. Hittite Microwave Corp. will show the benefits of using its new LO in a communication system demonstration.

### **Clock Generator**



Hittite recently released a new 125 to 3000 MHz HMC1034LP6GE clock generator for use with ADC, DAC, FPGA, DSP and processor clocking applications. Hittite's clock generator noise floor is typically -165 dBc/Hz. Also recently released is the company's HMC1031MS8E clock generator that can be used with a low-cost VCXO to convert a typical 10 MHz input reference to an output of up to 500 MHz. This then provides an ideal reference input for an LO or clock generator. Hittite Microwave Corp. will show the benefits of using its new clock generation device in a communication system demonstration.

VENDOR**VIEW**www.hittite.com



### Florida RF Labs Booth 1704

**Stranded Center Conductor** 



Florida RF Labs' Lab-Flex S Family is a stranded center conductor version of its popular Lab-Flex product. It offers high flexure rates, increased durability and improved electrical stability over the solid center conductor designs and is especially well-suited for test set-ups as well as radar and antenna systems that require coaxial interconnects that are being subjected to constant motion. Designs up to 65 GHz.

### EMC Technology

**SMA Coaxial Attenuators** 



EMCTechnology has released the new 42 W series of high performance precision SMA coaxial attenuators. This product expands the company's current offering of coaxial products out to 18 GHz and is offered in values from 0 to 30 dB. In EMC tradition, this product is offered in commercial or high reliability versions. EMC coaxial attenuators are manufactured with a stainless steel body and standard SMA male/female interface. The rugged construction

of these devices ensures reliability and continuous performance in the most demanding environments.

VENDOR**VIEW**www.emc-rflabs.com

### Analog Devices Booth 1725 RF Driver Amplifier



ADI's booth will spotlight complete system solutions and demos of new offerings, including RF/IF amplifiers, frequency

synthesizers and data converters, including the industry first ADL5324 half-watt RF driver amplifier with dynamically adjustable bias and extended temperature range for wired and wireless applications. In addition, ADI will demo the ADRF660x series of mixers and ADRF670x series of modulators, which achieve a breakthrough level of integration, enabling LTE and 4G base station manufacturers to realize an unprecedented 60 percent reduction in board space and a significant savings on bill of materials costs.

www.analog.com/rf

### Millitech Booth 1809 GaN Power Amplifiers



The bar has been raised! Millitech now offers differentiating E-Band and W-Band solid-state power amplifiers able to achieve small size and high power never before realizable. From 0.5 W to over 10 W available.

www.millitech.com

### CTS Valpey Corp. Booth 1728

Power Dividers



CTS Valpey Corp.'s is VFPD400 series of 4-way 0° power dividers offer the designer excellent RF performance in a compact 3  $\times$  3 mm QFN. The design is a fully passive monolithic IC that provides extreme part-to-part repeatability. The VFPD400 series is a family of devices that span across the frequency range of 500 MHz to

4 GHz and provide excellent phase and amplitude balance, high isolation, low insertion loss and VSWR.

### **Oven Oscillators**



The DFO-SI is the latest in CTS Valpey Corp.'s line of oven oscillators (OCXO) and it is available in a miniature 9  $\times$  14 surface-mount package. The device offers tight stability ( $\pm 20$  ppb) over the frequency range of 10 to 50 MHz. The DFO-SI has an HCMOS output, 3.3 V supply voltage and uses significantly lower power (0.3 W) than the competition. It is ideally used in applications such as base stations, IP timing, femto-cell, LTE, network timing and synchronization.

www.ctsvalpey.com



# Don't Waste Time and Money Designing Your Own Filter Test Box

Get your hands on Micro Lambda's tunable bench test filter

The MLBF-Series bench top filter from Micro Lambda Wireless provides designers and test engineers an easy to use wideband filtering capability in design labs and test environments.

Engineers no longer have to do their own design with individual components. The MLBF-Series can be supplied as a wide band tunable bandpass or bandreject filter with frequency coverage from 500 MHz to 50 GHz. Tuning is accomplished via Mechanical Knob, Keyboard Input, USB or Ethernet.

### Get one today and simply plug it in and start testing!



For more information about the MLBF Series or other products, please contact Micro Lambda Wireless.

### See our complete line of YIG-Tuned filters



Mini-filters .5 to 10 GHZ



1" cube filters



Bandpass filters



Bandreject .5 to 22 GHZ

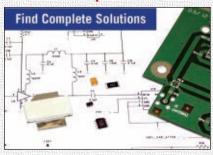
www.microlambdawireless.com



"Look to the leader in YIG-Technology"

# IMS PRODUCT SHOWCASE AISLES 1800-2200

### Richardson RFPD Booth 1818 Electronic Component Distributor



Richardson RFPD is a specialized electronic component distributor providing design engineers with deep technical expertise and localized global design support for the latest new products from the world's leading suppliers of RF, wireless and energy technologies. At the show, Richardson RFPD will offer a full schedule of presentations relating to new products, design tools and more. Stop by booth #1818 for insight into how you can accelerate time-to-market, find complete solutions, save development costs and, ultimately, improve design performance.

WENDOR**VIEW**www.richardsonrfpd.com

### West Bond

Booth 1901





West Bond Inc. is pleased to present one of the most popular manual machines made today. The 747677E-79 Triple Combination Wire Bonder: Wedge, Ball, and Ribbon. Since 1966, West Bond has been a designer and manufacturer of assembly and test equipment for the microelectronic industry. Including automatic, semiautomatic and manual ESD protected bonders, with ultrasonic, thermosonic, and thermocompression wire/ribbon capability. Included in its product line are eutectic and epoxy die bonders, insulated wire bonders, and pull testers with the company's patented X-Y-Z, 8/1 ratio micromanipulator.

www.westbond.com

### B&Z Technologies Booth 1927

### **Amplifiers**



B&Z Technologies is pleased to announce it's new "BZE" series of amplifiers for the EMC measurement market. These new

amplifiers are specifically designed to resist damage

to the input gain stages that is a common occurrence with amplifiers used for this application. Using "BZE" amplifiers for EMC receive testing will significantly reduce measurement interruptions typically caused by amplifiers damaged by ESD or other out of range signals at the amplifier input. The BZE-0118-251035-252520 0.1 to 18 GHz amplifier has a 2.3 dB typical noise figure, 35 dB minimum gain, 10 dBm output P1 dB and 2.5:1 VSWR.

www.bnztech.com

### Micro-Coax Inc. Booth 2024 Self-Locking Connectors



MICRO-COAX introduces Safe-D-LOCK technology that allows SMA, 2.92, 3.5 mm and other threaded connectors to lock against D-flat connectors of the same series. Unlike other solutions that only lock to the cable, Safe-D-LOCK offers resistance to cable installation torque and acceleration forces imparted on the cables. The result is a reliable, locked connection without the addition of adhesives, safety wires or other staking means. Best of all, Safe-D-LOCK's simplicity allows economical implementation, with few added components and no envelope enlargement.

www.micro-coax.com

Let this month's Product Showcase help you fill-in the Scavenger Hunt questions on page 282.

### **Empower** RF Systems

Booth 2203

### Amplifier and Switch Filter Bank

Empower model 2066-BBS3K4AUU delivers I kW power over the frequency band 500 to 1000 MHz. The amplifier and switch filter bank



that will be on display is constructed within one single 5RU drawer including the forced air-

cooling. The system can be configured for 180 to 260 VAC single phase supply or a three phase AC supply. An embedded web server allows for network management and control via the unit's Ethernet port connection. A web browser and the unit's IP address (IPV6) allows ease of access with the benefit of multilevel security.

WENDOR**VIEW**www.empowerrf.com

### SPINNER Atlanta Booth 2208 Compact Calibration Kits



The combination of all calibration standards in one handy unit is the optimum solution for simple, comfortable handling during

the calibration of network analyzers with the methods OSL and OSLT. The ergonomic arrangement of the components, small size and low weight are appreciated. The company's 4-in-1 calibration kits include open, short, load and through-line for the complete calibration of a network analyzer with two or more ports. The company's 3-in-1 calibration kits include all necessary standards for a complete OSL calibration of single port network analyzers.

www.spinner-group.com

### Teledyne Microwave Booth 2115

### **Broadband Amplifiers**



Teledyne Microwave Solution's new line of medium-power broadband amplifiers is a unique family of performance-based solutions designed for demanding applications. This family covers 20 to 2600 MHz and uses GaN technology. Each amplifier is hermetically sealed and includes multiple RF performance options so engineers can specify standard catalog or custom-tuned performance. The amplifiers include an internal sequencer, assuring application of the proper gate voltage applied to the FET prior to voltage applied to the drain. Higher gain versions include pre-amps, providing excellent noise figure and IP performance. The small package footprint is designed for high performance applications and operates from -40° to +85°C.

www.teledynemicrowave.com

### Teledyne Storm Products

### **Test Cable**



Introducing DuraTest, an extra durable, general purpose 0.180" test cable operating to 26.5 GHz with SMA SP connectors. With the proven toughness of Storm RF cable, captivated stainless steel connectors, and Storm's proprietary Hard-To-Hurt strain relief technology, Du-

raTest assemblies have a minimum flex life of 50,000 cycles and provide connector retention of 40 lbs min. Assemblies available for next day shipment in standard lengths, with any combination of SMA SP and N SP connectors. Phase matching available on request.

www.teledynestorm.com





## Hermetically Sealed Adapters

2.92mm, TNC, N, Feedthroughs with venting holes for Vacuum Test Chambers





Blg and Sman,
we have 'em all
Almost any Waveguide to almost any Coax Connector
WG Materials: Aluminum, Copper, Brass
Connectors: 1.92mm ...SMA....
TNC....N...7/16

www.spectrum-et.com

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Telephone: +49-89-3548-040 See us at IEEE MTT-S IMS Booth #1917 Facsimile: +49-89-3548-0490

### **IMS PRODUCT SHOWCASE AISLES 2200-2400**

### Reactel Booth 2210 **Small Form Factor Filters**



Reactel will feature a line of small form factor filters that are suitable for densely populated boards, portable systems or any application where size is at a premium. These

tiny units are available in discrete component, ceramic, cavity or combline designs. With profiles as low as 1/8" these robust units pack all of the performance of their larger counterparts into a much smaller package. They are available across a frequency range of 100 MHz to 20 GHz with bandwidths of 5 to 100 percent and are available in 4 to 12 sections

**VENDORVIEW** www.reactel.com

### San-tron PIM White Paper



Stop by booth #2219 and pick up a copy of San-tron's latest white paper, "Minimizing PIM Generation From RF Cables and Connectors." This is an extremely practical white paper on passive intermodulation (PIM), its effects on modern com-

Booth 2219

munication systems, and how it can be minimized in high-frequency cables, connectors and cable assemblies.

**VENDORVIEW** www.santron.com

### Werlatone

Booth 2236

### **Combiners and Directional** Couplers



Werlatone's high power combiners and directional couplers include a new product line, supporting a full 20

to 1000 MHz bandwidth. The new, low loss combiners address power requirements ranging from 10 to 500 W CW and tolerate severe power unbalances, while maintaining excellent port-to-port isolation. The company's new line of dual-directional couplers provides a low loss solution for broadband amplifier manufacturers seeking nonconnectorized couplers at the module level or connectorized components at the amplifier output. These broadband units are a perfect fit for military and commercial applications.

**V**VENDOR**VIEW** www.werlatone.com

### Aeroflex/ Weinschel

Booth 2305

### **Bidirectional High Power Fixed Attenuator**



This new convection cooled design operates from DC to 6 GHz frequency range with power handling up to 200 W average (Bidirectional) and 10 kilowatt peak (5 usec pulse width; I percent

duty cycle). Model 251 is designed to meet environmental requirements of MIL-DTL-3933 and is RoHs complaint. Available in 10, 20, 30 and 40 dB values with a choice of Type N male/female connector combinations. Other electrical specifications include VSWR of 1.20 maximum and a deviation over frequency of ±1.5 dB (maximum) across the operating frequency band.

**VENDORVIEW** www.aeroflex.com

### International Manufacturing Booth 2310 Services

### **Resistive Splitters**



International Manufacturing Services Inc. (IMS) announces the availability of the IPS Series - wideband two, three and four-way resistive splitters. The two-way (6

dB) resistive splitter functions optimally from DC to 20 GHz with accuracy starting at  $\pm$  0.5 dB while the three-way (9.5 dB) and four-way (12 dB) splitters function from DC to 7 GHz with accuracy starting at ±0.7 dB. These devices are available for surfacemount, microstrip or wirebond. Rated power is as high as 3 W.

www.ims-resistors.com

### State of the Art Booth 2325

### **Chip Resistors**



State of the Art Inc. (SOTA) announces its Z Termination line of miniature, high reliability chip resistors. The resistors range in size

from 0402 (0.040" × 0.020") to 2512 (0.025" × 0.025"), with tolerances from 0.1 percent, power ratings from 50 to 1500 mW temperature coefficients of resistance as low as 25 ppm, and voltage ratings from 30 to 200 V. The operating range for these resistors is from -55° to +125°C The Z Termination is a gold over nickel finish which can be attached with solder, conductive epoxy or gold wire bonds.

www.resistor.com

### LPKF Laser & Electronics

Booth 2409

### **UV Laser System**



Create PCBs on-demand right in the electronic lab with the LPKF ProtoLaser U3. This affordable UV laser system quickly processes a wide variety of material substrates and applications without the use of tools or chemicals, and switches between projects with a little

more than a click of the button. From cutting/depaneling any material from flex to fired ceramics, to drilling, skiving, decaping, and direct surface metal etching of the artwork, the ProtoLaser U3 has the ability to process applications that were previously only possible with the help of large and expensive industrial systems.

www.lpkfusa.com

### Rohde & Schwarz **Booth 2415**

### ZNB Network Analyzer



The four-port R&S ŻNB models cover the frequency ranges from 9 kHz to 4.5 GHz or 8.5

GHz. Rohde & Schwarz has designed the powerful instruments for demanding applications in the production and development of RF components with multiple ports. Two internal signal sources and a frequency-converting mode enable comprehensive measurements on mixers or amplifiers. Using mixed-mode S-parameter measurements, the R&S ZNB fully characterizes even balanced DUTs such as SAW filters used in mobile phones. Users benefit from the extremely wide dynamic range, short measurement times and exceptionally easy operation.

### Signal Generator



Rohde & Schwarz has enhanced its R&S SMB100A by adding new frequency options: The analog mid-range signal generator can now handle everything from analog RF to microwave applications. The R&S SMB-B120/B120L and R&S SMB-B140/B140L options (L versions without step attenuator) enable the generator to cover the frequency range from 100 kHz to 20 GHz and 40 GHz, respectively. In the new frequency ranges, the R&S SMB100A still offers a very wide dynamic range of -120 dBm to +14 dBm as standard. New high power options make it possible to achieve an output power of max. +25 dBm.

**VENDORVIEW** 

www.rohde-schwarz.com

# Purity & Precision Speed & Ease Rohde & Schwarz FSW

The most advanced signal and spectrum analyzer for aerospace and defense applications. The highest bandwidth, lowest phase noise, clearest user interface and a host of convenient new tools — all on the largest touchscreen available. The R&S°FSW is the perfect analyzer for testing all types of radar signals in aerospace and defense. Execute the most complex measurements with ease. See things that were previously undetectable. Go where no one has been before. The R&S°FSW. Compatible with today's technology. Built for tomorrow.

- Analyze oscillators and synthesizers with a phase noise of -137 dBc (1 Hz)
- I Measure frequency-hopping and chirp signals with a bandwidth of up to 160 MHz
- I Find spurious signals five times faster
- I Measure pulses, spurious and modulation at the same time with MultiView
- I See more and obtain faster results on the large touchscreen

The R&S®FSW. **Create the future**. www.rohde-schwarz.com/ad/fsw





# IMS PRODUCT SHOWCASE AISLES 2400-2600

### Networks International Corp. Booth 2418

### C-Band Filter/LNA



NIC introduces a ruggedized C-Band filter/LNA for use in eliminating interference caused by navigational communications (radar) of commercial and military aircraft, as well as coastal and marine vessels operating above and below the C-Band. This filter/LNA operates in the 4200 to 4600 MHz band and offers 23 dB gain, low noise figure of 1.1 dB, high selectivity and phase matching as low as  $\pm 1^{\circ}$  in a hermetically sealed package.

VENDOR**VIEW** 

### Micable Inc.

### Booth 2429

### **Cable Assemblies**



CO4 series is highly reliable and cost-effective cable assemblies, ideal for broadband tests and various connections. The triple-shielded cable has rugged construction employing an advanced strain relief system and is equipped with reinforced stain-

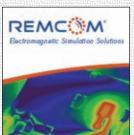
less steel connectors. They are so tough to be qualified for over 20,000 flex cycles without any change in electrical performance up to 18 GHz. They are available in custom lengths with SMA or N type connectors. You can rely on CO4 for daily test operation to repeatedly connect and disconnect.

www.micable.cn

### Remcom Inc. Booth 2430

### **EM Simulation Software**

Remcom introduces its XFdtd, a 3D EM Simulation Software for microwave device design and analysis. Whether the application is waveguides,



power dividers, filters, or couplers, XFdtd can provide quick, efficient and accurate simulation results. Visit Remcom's Microwave Application web page for a wealth of examples on power dividers,

circulators, Rotman Lens, and Waveguides: www.remcom.com/microwave-devices.

WENDOR**VIEW**www.remcom.com

### MECA Electronics Inc. Booth 2437

### Power Divider/Splitters



New low frequency range 2-, 3-, 4- and 9-way power divider/ combiners are optimized for excellent performance across all

bands from 5 to 500 MHz. Their rugged construction makes them ideal for all low frequency systems. Always available from stock — four weeks ARO in N and SMA connector configurations. Made in the USA — 36 month warranty.

WWW.e-meca.com

### Communications & Power Industries Booth 2438

### **Power Amplifier**



CPI introduces the VSS3610, a high-power S-Band solid-state power amplifier using 1300 W modules, effipower ciently combined. The 1300 W peakpower modules utilize state-ofthe-art GaN HEMTs for the most

and efficient design. The VSS3610 is designed to produce a very reliable air-cooled amplifier for mobile radar requirements, including Air Traffic Control radar systems. Standard peak power ranges from 7 to 25 KW (or higher).

www.cpii.com/bmd

### Z-Communications Inc. Booth 2528

### **Ultra-Miniature VCO**



Z-Communications Inc. introduces the USSP2450-LF for demanding portable radio applications. The ultra-miniature USSP2450-LF generates frequencies between 2400 to 2485 MHz within a control voltage range of 0.5 to 2.5 V DC making it enticing for PLL designs needing a low cost, high quality performance VCO in the 2.4 GHz ISM band. This oscillator measures a mere 0.2" × 0.2" × 0.07" and provides an SSB spectral purity of -82 dBc/Hz, typically, at 10 kHz while only drawing 6 mA of current from a 2.7 V DC supply.

www.zcomm.com

### Ophir RF Booth 2602 RF Amplifier



This class A RF power amplifier operates in a frequency range from 2 to 6 GHz and offers 100 W minimum

output power. This is the perfect choice for test measurement systems needing high power in the smallest commercially available package possible. This RFPA is backed by a three year warranty and Ophir RF's commitment to total customer satisfaction.

www.ophirrf.com

### Ciao Wireless Booth 2606 Broadband Amplifiers

Ciao Wireless introduces its line of high power, broadband amplifiers covering 0.5 to 20 GHz, I to 20 GHz, 2 to 20 GHz, and 2 to 22 GHz



with Output Power Levels up to +30 dBm at I dB PT. Various operating voltage levels are

available. Delivery is two to four weeks ARO & Ciao can customize any unit to meet your exact gain, noise figure, VSWR, and size requirements.

www.ciaowireless.com

# Crane Aerospace & Electronics Microwave Solutions Booth 2610

### **Beamforming Networks**



Crane Aerospace & Elec-Microtronics wave Solutions offers a wide range of beamforming products for advanced antenna and beamsteering applications Utilizing lumped element

(toroid), stripline or Multi-Mix® technology, frequency ranges from 50 MHz to 26 GHz are supported. Simple two port types to many input and output ports can be provided with the advanced fabrication and test technologies offered. Applications include directional signal reception for intercept applications, radar beamforming for phased array and directional applications and signal geolocation. All designs are custom and tailored to customer's specific requirements. Exceptional performance is obtained through careful CAD designs and critical process control.

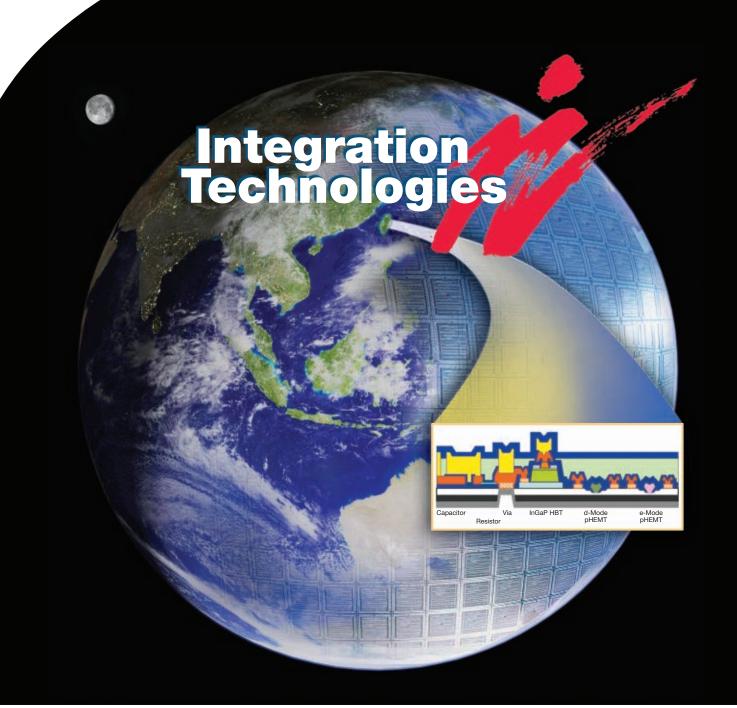
www.craneae.com/mw

### Weinschel Associates

### Booth 2616

### 100 W Attenuators and Terminations

Weinschel Associates introduces a line of 100 W attenuators and terminations designed to improve flexibility for integrators with a new cylindrical



### Innovative GaAs integration technologies without compromise

# HBT + pHEMT @ WIN = H<sup>2</sup>W e-Mode + d-Mode pHEMT @ WIN = e/d

It's a **whole new world** for designers with breakthrough integration technologies from WIN Semiconductors.

Combining GaAs HBT, enhancement and depletion pHEMT technologies on a single wafer enables innovative, highly integrated product solutions.

www.winfoundry.com

See us at IMS Booth 2816



### **IMS PRODUCT SHOWCASE AISLES 2700-3200**



body. Supporting a wide range of attenuation values (up to 30 dB in a bidirectional configuration and from 40 to 50 dB in a unidirectional design), the standard WA26 attenuator and WAT432 termination operate over the DC to 4 GHz frequency band with extended frequency operation up to 10 GHz available. The new body design enhances the

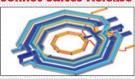
ability for this attenuator/termination to interface seamlessly with cable configurations where a rectangular body might complicate mounting.

www.weinschelassociates.com

### **Sonnet Software**

### **Booth 2702**

### Sonnet Suites Release 13



Visit Sonnet's booth for a free 20-minute, hands-on training class featuring its Sonnet Suites Release 13. Take a class and receive a complimentary Sonnet LitePlus license (\$495 value). The Sonnet Suites Release 13 features up to 3X faster analysis for large circuits, diago-

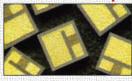
nal ports and components, smart via array meshing, and enhanced integration to Sonnet's EDA partners.

www.sonnetsoftware.com

### Tecdia Inc.

### Booth 2806

### **Dual Function Chip**



Combining a SLC capacitor and thin film resistor on a single ceramic chip is a Tecdia innovation that pays big dividends. The IRC or integrated resistor and capacitors are available in a variety of sizes and values to help engineers shrink designs, improve installation efficiency and lower material cost with su-

perb quality. These parts can be customized to your specific application. Visit booth #2806 to discover this and other space saving designs for your demanding applications.

www.tecdia.com/us

### Southwest Microwave Inc.

### Booth 2910

### **End Launch Connector**



Southwest Microwave's High Performance 1.85 mm End Launch Connector is now offered with a 5 mil diameter launch pin. This high performing connector is designed to provide low VSWR, wideband response up to 67 GHz for single-layer or multi-layer printed circuit boards where the microwave layer is on top. It is ideally suited for high frequency chip set evaluation/demo boards, test fixtures and board characterization. It provides optimum performance when

board launch geometry is grounded coplanar (CPWG) or top ground microstrip. The connector requires no soldering, is repairable and reusable.

www.southwestmicrowave.com

### **Narda**

### Booth 2916, 2917

### Two-Way Power Divider



The new Narda model 2372A-2 high-power, two-way power divider operates from 500 MHz to 2.5 GHz, handles up to 250 W CW input power (2 kW peak power) and provides exceptional phase and amplitude balance. This unit also operates as a non-coherent 125 Watt-per-signal power combiner. Currently in production, the unit incorporates proprietary high-power, thin-film resis-

tors that ensure broadband impedance matching and high isolation between inputs when used as a combiner rather than a divider. Model 2372A-2 measures just 3.5" × 2.5" × 1".

### **Holzworth Instrumentation**

### Booth 2926

### **Synthesis and Phase Noise Analysis**



Holzworth Instrumentation is a global provider of high performance RF synthesis and phase noise analysis products. Holzworth's broadband (250 kHz to 20 GHz) RF synthesizer module designs are based on a proprietary non-PLL architecture that is optimized for ultimate stability, switching speed and ultra low phase noise performance. Holzworth's

phase noise analyzer products are of the same innovative design philosophy optimized for speed, accuracy and reliability. Exciting new products will be launched at IMS 2012. Visit the Holzworth booth for a live demo.

www.holzworth.com

### **Logus Microwave**

### Booth 3006

### **Waveguide Switch**



The LOGUS WR10 ultra-light waveguide switch operates across the 75 to 110 GHz band and boasts a maximum VSWR of 1.20:1. insertion loss of 0.40 dB maximum and a minimum Isolation of 50 dB. The switching time is 50 ms maximum and it is available with

indicators, TTL interface control and 3 or 4 Port configurations. The Ultra-Light Series from Logus can be Airborne Application constructed and is also available from WR10 thru WR112 and Double-Ridge WRD180 thru WRD750.

www.logus.com

### **Greenray Industries Inc.**

### Booth 3206

### **TCXO**



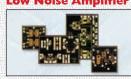
The T72 incorporates a rugged 5 × 7 mm ceramic package and a high performance crystal from Greenray's sister company Statek. The T72 offers stability to ±0.2 ppm (-40° to +85°C), g-Sensitivity of  $\leq 2.5 \times 10^{-9}/g$ , a phase noise floor of -155 dBc/Hz (typ.10 MHz), and very low current consumption to 1.9 mA (typ. with clipped sine output). A low

g-sensitivity option to  $\leq 7 \times 10^{-10}$ /g is available. The T72 TCXO, available from 10 to 50 MHz, offers clipped sine wave output and 3.3 V supply voltage.

www.greenrayindustries.com

### **Custom MMIC Design** Low Noise Amplifier

### Booth 3210



Stop by booth #3210 to learn about Custom MMIC's growing IP design library. Their latest product is a high efficiency GaAs low noise amplifier. The CMD I 62 boasts a noise figure of 1.7 dB with a small-signal gain of 22 dB. It reduces typical industry DC power dis-

sipation from approximately 160 mW down to 50 mW. The simplified design requires only positive drain and gate voltages, thereby eliminating complicated sequencer circuits commonly associated with LNAs in this range.

**VENDORVIEW** www.custommmic.com

### **Two-Way Power Divider**



The new Narda model 2382-2 high-power, two-way power divider operates from 500 MHz to 6 GHz, handles up to 250 W CW input power (2 kW peak power) and provides exceptional phase and amplitude balance. This unit also operates as a non-coherent 125 Watt-per-signal power combiner. The unit incorporates proprietary high-power,

thin-film resistors that ensure broadband impedance matching and high isolation between inputs when used as a combiner rather than a divider. Model 2382-2 measures just  $3.5" \times 2.5" \times 1"$ . This unit will be available in late summer 2012.

VENDORVIEW www.nardamicrowave.com

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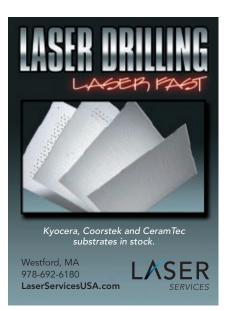
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# IMS PRODUCT SHOWCASE AISLES 3200-3300

# Charter Engineering Inc. Booth 3217 SPI2T RF Switch



CEI model S12P-141518 is a SP12T latching switch with indicator circuitry operating from DC to 13 GHz.

The ultra low PIM switch features a –160 dBc minimum 3rd order IM. The \$12 series is also offered as a failsafe or normally open switch along with various actuator and mounting options. CEI has been a leading producer of low PIM switches for over 10 years. The low PIM specifications are available with all CEI switches. Delivery: stock to two weeks.

www.ceiswitches.com

### Jackson Labs Booth 3219 Chip Scale Atomic Clock



The CSAC GPS-DO is the first commercial Chip Scale Atomic Clock (CSAC) available on the market. Jackson

Labs Technologies Inc. teamed with Symmetricom to integrate its Sa.45s CSAC into the CSAC GPS-DO module. This technology culminates from decades of research sponsored by the U.S. Government. The breakthrough technology allows a Cesium Vapor Cell Atomic Reference Oscillator to be packaged in a unit smaller than legacy products, with more than an order of magnitude in power reduction, while out-performing many industry-standard Atomic Oscillators.

www.jackson-labs.com

### Advanced Test Equipment Rentals Booth 3220

### **Radiation Meter**



The Narda SRM-3006, the 9 kHz to 6 GHz selective radiation meter, has been specially developed as a frequency-selective measuring system for safety issues in electromagnetic fields. The operating modes are precisely tailored to the applications: Spectrum Analysis, Safety Evaluation UMTS P-CPICH Demodulation, Level Recorder, and Scope. Narda SRM-3006 is a complete measuring system: The

SRM-3006 basic unit detects and takes account of antenna and calibration data automatically, eliminating a common source of errors. A further advantage: all measuring antennas in the SRM family are mutually compatible. Antennas from other manufacturers can also be used with the Narda SRM-3006.

www.atecorp.com

# Precision Connector Inc. Booth 3303



Precision Connector Inc. has introduced a new line of precision connectors designed for 0.047 semi-rigid cable. Both 1.85 mm and 2.92 mm male and female connectors are available and have been designed for low VSWR and insertion loss. The 1.85 mm series performs to 65 GHz and the 2.92 mm series performs to 46.5 GHz. Both designs incorporate fully captivated center contacts with rear sockets that accept a pointed cable center conductor, eliminating the need for center contact soldering. A solder ferrule is used to attach the cable outer jacket to the main connector body with a threaded clamp nut. All bodies are manufactured from passivated stainless steel and contacts and solder ferrules are constructed from gold plated beryllium copper.

www.precisionconnector.com

### Norden Millimeter

### Booth 3326

### **Down Converter**

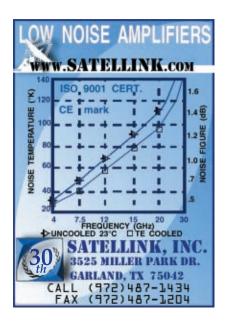


To assist system designers in expanding the frequency capabilities of their systems, Norden engineers have designed and are manufacturing a

24 to 40 GHz down converter with an integrated bypass to provide a single IF output covering the 0.8 to 24 GHz band. The IF frequency of the down converter is used as the input RF frequency for an ELINT receiver, such as the Norden ELINT receiver. Norden combines multiple assembly technologies with the latest MMIC and packaging technology to reduce size, weight and power, while maintaining superior performance.

www.nordengroup.com







See us at IMS Booth 2118



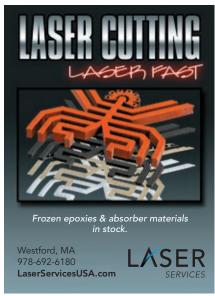
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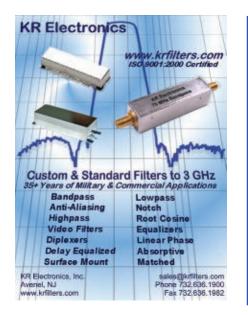
www.signalcore.com







See us at IMS Booth 215





Model LVC440-495VS tunes 440MHz to 495MHz and is used in handheld wireless RF applications. A bias voltage of 1.5V delivers + 2.0dBm power with only 5ma current consumption. Phase noise is -94dBc @ 10kHz offset. Package size is 0.175 inch square with height of .075 inch. Supplied on T&R and priced @ \$4.95 ea for 10k quantity.

www.modcoinc.com



# Canada

# Microwave Life Savers:

## Small Companies at IMS That May Keep You Afloat

t would be very difficult to see every booth at a tradeshow. But isn't it great to come away from a show with a hidden gem that you stumbled upon? Here are a few to put on your schedule. From components for infrastructure to custom MMICs for an aerospace/defense application, these companies just might be the solution you will need in a pinch this year.

If you have been anywhere near a base station lately, no doubt you or someone you know has uttered "passive intermodulation" or "PIM", more than likely with some angst. Unlike low-level noise, which tends to cover broad bandwidths, PIM results in discrete signals that fall within the operating bandwidth of a wireless communications receiver, capable of interfering with desired signals. At sufficiently high magnitudes, PIM distortion can desensitize a communications receiver, resulting in poor quality of calls or even dropped calls. To learn more about PIM and some simple, yet robust cable assembly solutions, stop by some of the industry leading cable companies. San-tron (booth #2219) will be demonstrating how their new line of low-PIM jumper cables deliver PIM performance of -158 dBc standing still and then when heavy vibration is applied, continues to remain extremely stable, degrading just 2 dB.

Does your specific application call for performance not available

in a catalog MMIC? Visit the team at Custom MMIC in booth #3210 to learn how attainable a uniquely designed MMIC can actually be. This particular design house offers three levels of engagement including access to their private stock of performance driven designs for rapid delivery. From singlefunction to multi-function, Custom MMIC is a good fit for companies that wish to outsource their design activity, especially when you need a custom design in a specific compound semiconductor technology such as GaAs, GaN, SiC or InP. Custom MMIC will be demonstrating their latest GaAs MMIC low-noise amplifier (LNA) chip optimized for 30 GHz satellite communications with a typical noise figure of 1.7 dB in their booth. With dozens of years of combined experience designing MMICs for microwave and millimeter-wave applications, it is worth a booth visit to talk about how your own unique design requirements could be realized.

LPKF in booth #2409 may be the biggest tease at the show. There is not an engineer in the business that would not want to have a machine on their bench that outputs their circuit ideas like a desktop printer. Don't believe me? Eighty-five percent of the respondents to Microwave Journal's April online poll question named the PCB prototype milling machine as the most important tool in their design

arsenal. I am talking about real boards. Boards that can be tested, tweaked and tried again, without the interruption of going outside to the board house. Sure, it would be great if you could grab one of these at Staples, but unfortunately these German-engineered laser machines cost a couple of bucks. But the payoff in design efficiency is immeasurable and the LPKF booth staff can show you how to sell the value of your productivity to even the stingiest CFO.

Moving from design to manufacturing, other companies using lasers to save the day are Laser Services in booth #215, Thunderline-Z in booth #601 and Litron in booth #2229. With the bulk of vendors highlighting new RF components, software and test instruments, its easy to overlook the smaller group of companies providing manufacturing services, but IMS is a great place to meet the folks who understand the special physical requirements that go into microwave products. Laser Services is an experienced high power laser job shop using YAG and CO2 lasers to perform any number of laser precise cutting, drilling, marking, etching and welding jobs for you. They maintain a stash of name brand alumina substrates and frozen epoxies and offer unique design-for-manu-

### **DAVID STRAND**

Strand Marketing, Newburyport, MA

European Microwave Week 2012 Amsterdam RAI, The Netherlands October 28<sup>th</sup> - November 2<sup>nd</sup> 2012





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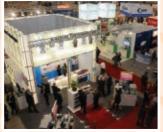
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# Canada

facturability solutions such as an innovative laser ablation technique for solder damming.

Many of the components found on the exhibition floor are used in harsh environments and require advanced packaging. Thunderline-Z opened their own laser center last year, focused on augmenting their full-service packaging services. Their solutions include laser lidding and testing of hermetic modules, and laser feedthru installation that will allow you to obtain some of the tightest pin-to-pin tolerances imaginable. Litron Inc. also provides laser welding, laser sealing and laser cutting services for

aerospace, industrial and medical components from hi-rel electronic microwave packages to class three medical implant devices.

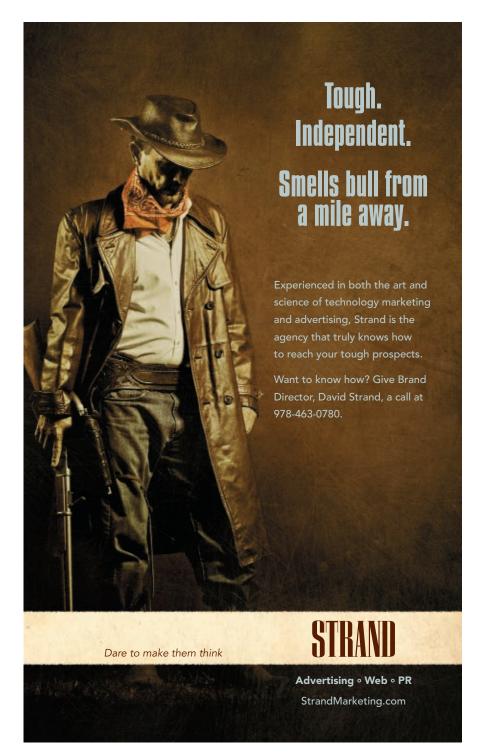
Speaking of harsh environments, are you working in space or just looking for space-level type design and manufacturing capabilities? Hi-rel multi-chip modules and RF semiconductor packaging solutions are a specialty of KCB Solutions in booth #3513. If you are concerned about thermal or electrical stability in high power applications, talk to them about their new weightless, void-free approach to eutectic die attach.

Wondering where you might possibly turn to handle overflow in production or high frequency test without going off-shore? SemiGen in booth #301 is the partner you're looking for. Microwave assembly and semiconductor packaging is an art that is not lost on this assembly house and they also offer you fast delivery of bonding supplies and diodes and capacitors from their own in-house RF Supply Center.

Speaking of high frequency testing, do you need a signal generator for your ATE set up, but do not need all the bells and whistles of a big brand piece of equipment? Lab Bricks from Vaunix in booth #1129 are a complete line of USB powered, miniature, yet robust, signal generators, attenuators and now an RF switch that are softwarecontrolled and easy to use. Each device comes with a USB flash drive containing the GUI software and digital version of the programming guide, along with a 6-ft. USB cable. The Lab Brick is compatible with NI's Labview so that you can easily incorporate them into your custom test set-up. Several small companies are now offering compact, USB powered testing solutions so look for them at the show.

Have a great show and let me know if I can dig up any other gems for you. ■

**David Strand** is CEO and Brand Director of Strand Marketing and a microwave industry insider. You can follow his insights on Twitter @ StrandMkt or reach him at dstrand@strandmarketing.com.



### **IEEE MTT-S IMS 2012 MicroApps Expert Forum**

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**Moderated by:** Dr. Larry Dunleavy, President and CEO of Modelithics, Inc.





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### The Book End



Antennas and Propagation for Body-Centric Wireless Communications

Edited by Peter S. Hall and Yang Hao

ntennas and Propagation for Body-Centric Wireless Communications, second edition, is updated and revised providing complete and current details on the theory, design and applications of wireless antennas for on-body electronic systems. The book offers readers brand new material on advances in physical phantom design and production, recent developments in simulation methods and numerical phantoms, descriptions of methods for simulation of moving bodies, and the use of the body as a transmission channel. There is also a completely revised chapter on channel characterization

and antenna design at microwave frequencies. This book includes the latest information for existing applications like Bluetooth headsets together with detailed treatment of techniques, tools and challenges in developing on-body antennas for an array of medical, emergency response, law enforcement, personal entertainment, and military applications on the horizon.

The book covers energy propagation around and into the body and how to estimate performance of on-body wireless links. Then it dives into the nutsand-bolts of designing antenna systems that deliver the goods. It covers on-body communication channels at microwave frequency bands and at low frequency bands, as well as ultra wideband systems for WPANs and WBANs. It also includes details on body-centric UWB antennas and channels, as well as advances in wearable mobile, EBG, and "smart fabric" antennas for cellular and WLAN communications. Chapters on

telemedicine applications, such as remote diagnoses and implantable medical devices cover crucial propagation issues and other obstacles that need to be addressed. Rounding out the coverage is a section on antenna design for body-sensor networks and their emerging military and space applications. The editors have gathered the latest information from noted experts in the field making this volume a very useful tool for engineers designing and improving body-centric communication systems.

### To order this book, contact:

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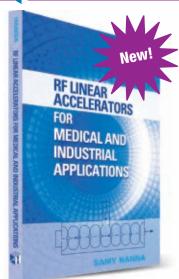
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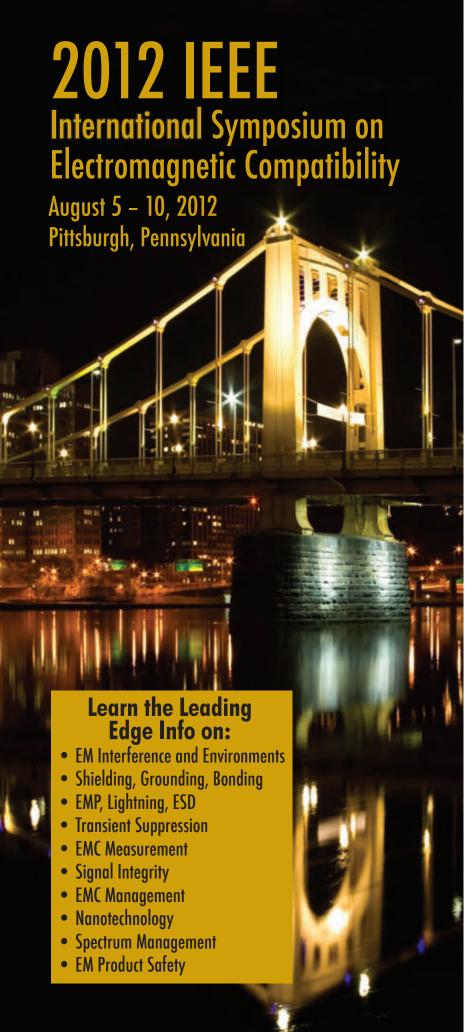
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### Coming in June:

Semiconductors/MMICs/RFICs

- MARKET OPPORTUNITIES FOR GAN: VIEWS FROM INDUSTRY EXPERTS
- · WIDE BANDGAP GAN POWERS HIGH SPEED WIRELINE NETWORKS
- TECHNIQUES FOR TIME SIDELOBE MEASUREMENTS

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Frequency Matters.

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# Enter the MWJ Puzzler Contest For a chance to Win a Kindle Fire!



Tuesday, June 19th at 4:00pm Wednesday, June 20th at 4:00pm Thursday, June 21st at 2:00pm

Drop off your Completed Puzzler Sheet at MWJ Booth #2018 You don't have to be present at the drawing to win (But then you'll miss all the fun)

### **IMS 2012 Products Scavenger Hunt**

See the next page for details and the form





# **IMS 2012 Scavenger Hunt**

An IMS exhibition attendee has a lot of vendors to visit in a short period of time. To find what you need, you need to know where to look. The missing term in the following sentences can be found among the vendors in this issue's IMS Product Showcase. Use the clue and look up the vendor's product description (pg. 250) by booth number to find the correct missing word.



<ol> <li>The is one of the first components after the antenna in the signal chain of a noise sensitive receiver. Find one by going to vendors in Booths 815, 1210, 1425 or 2418.</li> <li>To keep out unwanted signals, vendors in Booths 1728, 2236, 2916 and 3006 are displaying components with high</li> <li>If you need to extend the dynamic range of an instrument, you may need an from one of the vendors in Booths 601, 1129, 1704 or 2616.</li> <li>Component and test equipment manufacturers in Booths 112, 1015, 1300, 1600, 1607, 2926 and 3206 know the importance of providing their customers</li> </ol>	<ol> <li>Vendors in Booths 907, 1 magnetics to provide of your high frequency structions.</li> <li>A harmonic and Booth 1215.</li> <li>To understand and mit spurious signals due to and test solutions from ve and 3217.</li> <li>Anyone designing combenefit from using the Vector Analysis System available.</li> </ol>
with low  5. The solid outer metal sheath gives the offered by vendors in Booths 509, 514 and 3303 excellent shielding properties.	Bonus Puz Use the letters in this po
6. A can be realized in many technologies, from waveguide to semiconductors, but vendors in Booths 510, 1129, 1210 and 1507 will help you route your signals with minimal insertion loss into two signal paths.	more than once.

7.	Vendors in Booths 907, 1615 and 2430 use 3D electro-
	gnetics to provide
of y	our high frequency structures.

- 8. A harmonic and mixed-signal active \_\_\_\_\_ system can be found in Booth 1215
- **9.** To understand and mitigate the impact of in-band spurious signals due to \_\_\_\_\_\_, look for products and test solutions from vendors in Booths 1015, 2219, and 3217.

### **Bonus Puzzler Points**

Use the letters in this popular component to spell out a famous Canadian icon. Letters may be used more than once

**AMPLIFIER** 

Drop off the completed puzzler at MWJ Booth #2018 for a chance to win a daily drawing of a Kindle Fire.

Name:		
Mobile Phone:		
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### Sponsored By:



# As good as PTS synthesizers look on paper...

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20 µs frequency switching broadband



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Configure a system to fit your needs with our vast selection of options

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## 20-1000 MHz

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- Lowest Loss
- Excellent Port-to-Port Isolation
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- POWER COMBINERS/DIVIDERS
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- 0°/180° HYBRID JUNCTIONS

Werlatone, Inc. 17 Jon Barrett Road Patterson, New York 12563 T 845.278.2220 F 845.278.3440 www.werlatone.com

### In-Phase Combiners/Dividers

Model	Type	Frequency (MHz)	Power (WCW)	Size (Inches)	Insertion Loss (dB)	VSWR	Isolation (dB)
D6233	2-Way	10-1000	25	3.25 x 2 x 1.1	0.75	1.35:1	20
D8632	2-Way	20-1000	50	2.2 x 2.02 x 1.5	0.7	1,40:1	20
D8300	2-Way	20-1000	100	2.45 x 2 x 0.91	0.5	1.35:1	20
D8544W*	2-Way	20-1000	100	2.85 x 2.5 x 1	0.5	1.35:1	18
D8682	2-Way	20-1000	500	5.2 x 2.65 x 1.8	0.6	1.35:1	15
D8851W*	2-Way	20-1000	500	5.6 x 3.05 x 1.8	0.6	1.35:1	15
D7365	4-Way	20-1000	100	5 x 2 x 1	0.75	1,35:1	20
D7439	4-Way	20-1000	250	5 x 5 x 1.5	0.75	1.35:1	18
D8746	4-Way	20-1000	500	7.2 x 3.5 x 1.4	0.7	1.35:1	15
D9048	4-Way	20-1000	500	5 x 4.7 x 1.4	0.6	1.35:1	17

<sup>\* &</sup>quot;W" references a Watertight Design

### **Dual Directional Couplers**

Model	Coupling (dB)	Frequency (MHz)	Power (WCW)	Size (Inches)	Insertion Loss (dB)	VSWR	Directivity (dB)
C8858	40	10-1000	250	2.09 x 1.16 x 0.57	0.4	1.30:1	20
C8631*	40	20-1000	150	1.5 x 0.95 x 0.5	0.35	1.25:1	20
C8696	40	20-1000	150	1.76 x 1.16 x 0.57	0.35	1.25:1	20
C8686	40	20-1000	500	5.2 x 2.7 x 1.7	0.35	1.25:1	20

<sup>\*</sup> Non-Connectorized / Tabs

Our Patented, Low Loss designs tolerate high unbalanced input powers, while operating into severe Load Mismatch conditions.



## PRODUCT SELECTION GUIDE

Analog, Digital & Mixed-Signal ICs, Modules, Subsystems & Instrumentation, DC - 110 GHz

















### **Automotive**

**Telematics & Sensors** 

### **Broadband**

Cable Modem, CATV, DBS & VoIP WiMAX, WiBro, WLAN & UWB

### Cellular Infrastructure

GSM, GPRS, CDMA, TD-SCDMA, WCDMA, UMTS & 4G/LTE

### Fiber Optics & Networking

OC-48 to 100G

### Microwave & mmWave Communications

Backhaul Radio Links Multi-Pt Radios & VSAT

### **Military**

C3I, ECM & EW

### **Space**

**Payload Electronics** 

### Test & Measurement

Commercial & Industrial Sensors
Test Equipment







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### **CUSTOMER SUPPORT**



### How to Buy:

Hittite Microwave Corporation offers many convenient ways to order products and/or receive pricing and delivery information. Our order entry/MRP system assures customer sample requests and orders will be entered quickly, tracked easily, and completed accurately on-time.

#### **Direct Sales**

#### HMC Field Sales Offices:

You may contact our corporate or field sales offices listed on the back cover for assistance in purchasing Hittite products.

#### • Purchase On-line: www.hittite.com

With Hittite Microwave's E-Commerce capability customers can enjoy the convenience of on-line ordering via a secure shopping cart interface. Products can be purchased using either a MasterCard, Visa, American Express or JCB card. Orders are confirmed within one business day with delivery information. Orders ship within 2 business days of confirmation, based on availability.

#### • Purchase Orders via HMC Corporate Sales:

You may contact Hittite Microwave directly at (978) 250-3343. Purchase orders can be faxed to (978) 250-3373 or sent via email to <a href="mailto:sales@hittite.com">sales@hittite.com</a>. There is a minimum purchase order value of \$500.00 (U.S. Dollars).

#### **Worldwide Network of Sales Representatives**

You may purchase our products through our network of manufacturer representatives listed on the back cover.

- European customers may also purchase products in Euros (€) directly from Hittite Microwave Deutschland GmbH (germany@hittite.com).
- Japanese customers may also purchase products in Yen (¥) directly from Hittite KK - Japan (japan@hittite.com).

### **OUR QUALITY POLICY:**

#### **Hittite Microwave Corporation is Committed to:**

- Being a supplier of products of the highest quality.
- Advancing state-of-the-art technology to support our products.
- Enhancing our competitive position with superior products.

#### Hittite's Quality Policy Recognizes Responsibilities for Every Individual to:

#### Tresponsibilities for Every murrium

- Take the initiative to promote quality.
- Create an environment where the highest quality standards are maintained.
- Participate in continuous improvement practices.

### QUALITY & PRODUCT SUPPORT:

#### The Quality & Product Support Section of Our Web Site Includes:

- Quality Assurance -
- Product manufacturing, qualification & screening flows
- Product Reliability
- Qualification Test Reports

#### **Product Application Support**

- Application Engineering Support
- Application Notes
- Mixer Spur Chart Calculator, Parametric Search & PLL Phase Noise Calculator
- Product Cross Reference
- Package & Layout Drawings -

Product outline, PCB land pattern and tape & reel drawings

- Published Papers
- S-Parameter Files

### Data Sheets

Complete product data sheets can be found on our web site.

HMC is ISO 9001:2000, AS9100 and ANS/ESD S20.20-2007 certified. Every component is backed by every Hittite employee and subcontractor's commitment to total quality, thus providing our customers with products that meet or exceed all requirements, are delivered on-time and function reliably throughout their useful life.

### WHAT WE DO

Hittite Microwave Corporation is an innovative designer and manufacturer of high performance integrated circuits (ICs), modules, subsystems and instrumentation for technically demanding digital, RF, microwave and millimeterwave applications covering DC to 110 GHz. The Company's standard and custom products apply analog, digital and mixed-signal semiconductor technologies, which are used in a wide variety of wireless / wired communication and sensor applications for Automotive, Broadband, Cellular Infrastructure, Fiber Optics & Networking, Microwave & Millimeterwave Communications, Military, Test & Measurement and Space markets. We offer over 1025 products across 35 product lines.

#### RF & Microwave ICs

Amplifiers

Attenuators

Automatic Gain Control

DC Power Conditioning

Filters - Tunable

IF / Baseband Processing

I/Q Mixers/IRMs

I/Q Downconverter/Receivers

I/Q Upconverters/Transmitters

Mixers

Modulators/Demodulators

Phase Shifters

Power Detectors

SDLVAs

Switches

Transceivers

Variable Gain Amplifiers

### Analog & Mixed-Signal ICs

Broadband Time Delays Comparators

Crosspoint Switches

Crosspoint Swi

Data Converters

DC Power Conditioning

DC Power Management

High Speed Digital Logic

IF/ Baseband Processing

Interface

Limiting Amplifiers

Mux & Demux

Optical Modulator Drivers

Transimpedance Amplifiers

### Clocks & Timing ICs

Clock Distribution

Clock Generators

PLL with Integrated VCOs

#### LO Freq. Generation ICs

DC Power Conditioning

Filters - Tunable

Freq. Dividers & Detectors

Freq. Mulitipliers
Phase Locked Loop

PLL with Integrated VCOs

VCOs PLOs

#### **Connectorized Modules**

Amplifiers

Attenuators DROs

Frea. Dividers & Detectors

Freq. Multipliers

High Speed Digital Logic

I/Q Mixers

Mixers Phase Shifters

SDLVAs

Switches

Synthesizer Module, MicroSynth®

VCO

#### Instrumentation

Signal Generators

We design and supply custom analog and digital ICs, modules, subsystems and instrumentation, combining multiple functions for specific requirements. We select the most appropriate semiconductor and package technologies, uniquely balancing digital and analog integration techniques.

Our custom and standard products support a wide range of wireless / wired communications & radar applications for the following markets:



Automotive

Telematics & Sensors



Broadband CATV, DBS, WiBro, WiMAX, WLAN, Fixed Wireless & UW



Cellular Infrastructure GSM, GPRS, CDMA, WCDMA, UMTS, TD-SCDMA & 4G/LTE



Fiber Optic & Networking OC-48 to 100G



Microwave & mmWave Communications Backhaul Radio Links Multi-Pt Radios & VSAT



Military C<sup>3</sup>I, ECM & EW



Payload Electronics



Test & Measurement Commercial / Industrial Sensors & Test Equipment



### May 2012 - 21 New Products

#### **AMPLIFIERS** - Linear & Power

Frequency (GHz)	Function	Gain (dB)	OIP3 (dBm)	NF (dB)	P1dB (dBm)	Bias Supply	Package	ECCN Code	Part Number
9 - 13.3	2W Power Amplifier	34	42	5.5	33	+6V @ 1400 mA	Chip	3A001.b.2.b	HMC952
9 - 14	2W Power Amplifier	33	43	-	34	+6V @ 1400 mA	LP5G	3A001.b.2.b	HMC952LP5GE
33.5 - 46.5	0.5W Medium Power Amplifier	21	35	-	24.5	+6V @ 500 mA	Chip	3A001.b.2.d	HMC1014
27.5 - 33.5	1W Power Amplifier	24	40	-	29	+6V @ 600 mA	Chip	3A001.b.2.d	HMC1024
29 - 37	2W Power Amplifier	22	42	6	32	+6V @ 1200 mA	Chip	3A001.b.2.d	HMC1029
24 - 43.5	Low Noise Amplifier	23	22	2.3	12	+2.5V @ 70 mA	LP3C	3A001.b.2.d	HMC1040LP3CE

#### **CLOCKS & TIMING**

#### **Clock Distribution**

Max. Clock Rate (GHz)	Function	Input	Output	Phase Jitter (12 k to 20 MHz)	Rise/Fall Time (ps)	Channel Skew (ps)	Disable Mode	Power Supply (V)	Package	ECCN Code	Part Number
4	Clock Divider & Delay Management	LVPECL, LVDS, CML, CMOS	LVPECL	13 fs RMS	90	300 to 1500	Yes	5 or 3.3	LP3	3A001.a.11.b	HMC988LP3E

#### **Clock Generators**

Max. Frequency (MHz)	Function	Typical Phase Jitter (fsRMS)	Phase Noise Floor (dBc/Hz)	Maximum Reference Freq. (MHz)	Typical Power Consumption (W)	Figure of Merit (Frac/Int) (dBc/Hz)	Package	ECCN Code	Part Number
500	Integer Mode PLL (x1, x5, x10)	Defined by VCXO	Defined by VCXO	140	0.0064	-208	MS8	EAR99	HMC1031MS8E

#### **DATA CONVERTERS**

#### Low Power Analog-to-Digital Converters

Sample Rate	Function / Mode	Resolution (bits)	# of Channels	Power Dissipation	SNR (dBFS)	SFDR (dBc)	Package	ECCN Code	Part Number
20/40/50/65 MSPS	Octal Channel	10	8	12/20/25/30 mW / Channel	61.6	81	LP9E	EAR99	HMCAD1104

#### Ultra High Speed Analog-to-Digital Converters

Input Frequency (GHz)	Function	Sample Rate (Gsps)	Resolution (Bits)	ENOB	SFDR (dBFS)	Package	ECCN Code	Part Number
20	3-Bit ADC with 1:2 Demux	26	3	2.9	26	LP9	3A001.a.11.b	HMCAD5831LP9BE

### Track-and-Hold Amplifiers

Input Frequency (GHz)	Function	Single Tone THD/SFDR (dB)	Maximum Clock Rate (GS/s)	Output Noise (mV RMS)	Hold Mode Feed-through Rejection (dB)	Package	ECCN Code	Part Number
DC - 18	Track-and-Hold	-65 / 67	4.0	1.65	> 60	LC4B	3A001.a.11.b	HMC661LC4B
DC - 5	Track-and-Hold	-65 / 67	4.0	0.86	> 60	LC4B	3A001.a.11.b	HMC760LC4B

### DC POWER MANAGEMENT - Active Bias Controller

Supply Range (V)	Function	VDRAIN Range (V)	IDRAIN Bias Current (mA)	IGATE Drive Current (mA)	VGATE Range(V)	Over/Under IDRAIN Current Alarm	Package	ECCN Code	Part Number
5 - 16.5	Active Bias Controller	5 - 16.5	50 - 1600	-4 to 4	-2.46 to +2.04	Yes	Chip	EAR99	HMC980

#### FILTERS - Tunable

### Programmable Harmonic

Frequency Range (GHz)	Function	Return Loss (dB)	3 dB Bandwidth(GHz)	Stopband Frequency (Rej. >10 dB)	Tuning Response (ns)	Package	ECCN Code	Part Number
0.25 - 3.025	Programmable Harmonic Low Pass	10	1 - 3	1.2 Fcutoff	10	LP3	EAR99	HMC1044LP3E

#### **Band Pass**

Frequency Range (GHz)	Function	Return Loss (dB)	3 dB Bandwidth (%)	Low Side Rejection Frequency (Rej. >20 dB)	High Side Rejection Frequency (Rej. >20 dB)	Tuning Response (ns)	Package	ECCN Code	Part Number
9 - 19	Band Pass	9.5	18	0.81 x Fcenter	1.17 x Fcenter	200	Chip	EAR99	HMC897

### I/Q Mixers / IRMs

RF Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	LO / RF Isolation (dB)	IIP3 (dBm)	Package	ECCN Code	Part Number
15 - 33.5	I/Q Mixer / IRM	DC - 3.5	-10	40	22	LC4	EAR99	HMC1042LC4

### MIXERS - Downconverter RF ICs & +13 to +14 dB LO Double & Triple Balanced

RF Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	LO / RF Isolation (dB)	IIP3 (dBm)	Package	ECCN Code	Part Number
0.7 - 3.5	High IP3 Dual Downconverter	0.05 - 0.35	7	55	+25	LP4	EAR99	HMC990LP4E
2 - 18	Double Balance Mixer	DC - 2	-10	35	19	LC3B	EAR99	HMC91048LC3B

### **OPTICAL MODULATOR DRIVERS**

Data Rate Max. (Gbps)	Function	Gain (dB)	Group Delay Variation (ps)	Additive Jitter (ps)	Output Voltage Max. (Vp-p)	Package	ECCN Code	Part Number
32	8Vpp Optical Modulator Driver, SMT Package	32	+7	0.25	8	BGA	EAR99	HMC5850BG

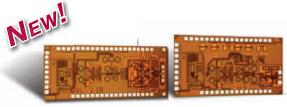
### TRANSCEIVERS - New Product Line!

Frequency (GHz)	Function	P1dB (dBm) NF (dB)	Max Gain (dB)	Gain Adjust (dB)	Phase Noise @ 1 MHz Offset (dBc/Hz)	Power Dissipation (W)	Package	ECCN Code	Part Number
57 - 64	60 GHz Integrated Transmitter	12 dBm	38	17	-86	0.8	Chip	5A991.b	HMC6000
57 - 64	60 GHz Integrated Receiver	6 dB	67	65	-86	0.61	Chip	5A991.b	HMC6001



### **New & Expanded Product Lines**

### HMC6000 & HMC6001 Millimeterwave Transmitter & Receiver ICs, 57 - 64 GHz



### Supports WiGig & IEEE 802.11ad **Multi-Gbps Solutions!**

### Rx Noise Figure & Tx P1dB vs. Frequency (Maximum Gain) 18 (dBm) 16 14 NOISE FIGURE (dB) & P1dB 12 10 8 6 4

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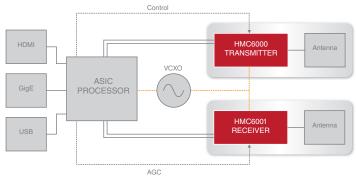
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FREQUENCY (GHz)

#### Features

- ♦ Covers 57 64 GHz Frequency Band
- ♦ Complete Baseband to RF Solutions
- ♦ Integrated Frequency Synthesizer
- ♦ Universal Analog I/Q Baseband Interface
- ♦ Up to 1.8 GHz RF Bandwidth

#### **INDOOR Gbps LINKS**



Highly Integrated IC Radio Solutions for Low-Cost 60 GHz Applications!

### HMC1044LP3E Industry's First Programmable Harmonic Filter Ideally Suited for Multi-Standard, Multi-Carrier Applications

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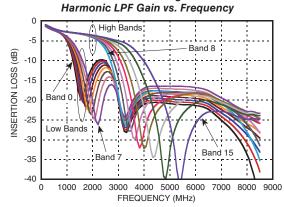


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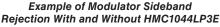
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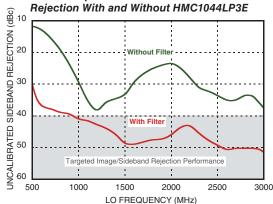
### HMC1044LP3E for Programmable



### **Features**

- ♦ Programmable Bandwidth to Track Wideband Sources to 3 GHz
- ♦ 20 dB Typical LO Harmonic Rejection Improves Modulator/Demodulator Sideband/Image Rejection
- ♦ Integrated Filter, No Calibration Required
- ♦ Footprint up to 90% Smaller than Fixed **Passive LO Filters**





Reduced Harmonic Content Dramatically Reduces Sideband Rejection When Driving Wideband Quadrature Mixers!



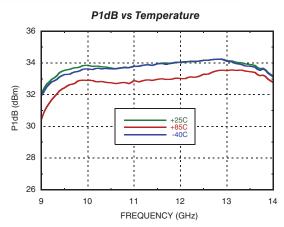
### **New & Expanded Product Lines**

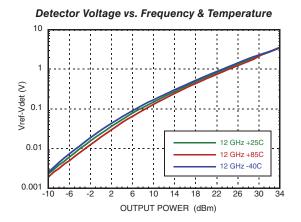
### HMC952LP5GE GaAs pHEMT MMIC 2W Power Amplifier with Power Detector, SMT, 9 - 14 GHz



### **Features**

- ♦ High P1dB Output Power: +34 dBm
- ♦ High Psat Output Power: +35 dBm
- ♦ High Gain: 33 dB
- ♦ High Output IP3: +43 dBm
- ♦ Supply Voltage: Vdd = +6V @ 1400 mA





Ideal for High Linearity Microwave Radio, Military SATCOM Applications!

### HMC990LP4E Broadband High IP3 Dual Channel Downconverter, 0.7 - 3.5 GHz

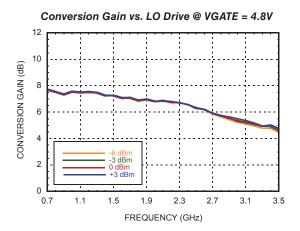


### Compact Solution, 4 x 4 mm<sup>2</sup> QFN Package!

#### Input IP3 vs. High Side LO & Low Side LO @ VGATE = 4.8V 31 29 27 25 IP3 (dBm) 23 21 19 High Side LO 17 15 0.7 1.5 1.9 2.3 2.7 3.1 1.1 FREQUENCY (GHz)

#### **Features**

- ♦ 0.7 3.5 GHz Broadband Operation with No External Matching
- ♦ High Input IP3: +25 dBm
- ♦ SSB Noise Figure: 9 dB
- ♦ Power Conversion Gain: 7 dB



Ideal for Multi-Standard Cellular Base Station and Wideband Radio Link Receivers!



### SMT & Chip (Die) Products

requency (GHz)	Function	Gain (dB)	OIP3 (dBm)	NF (dB)	P1dB (dBm)	Bias Supply	Package	ECCN Code	Part Number
ow Noise Ar	nplifiers	(, ,	(° )	(* /	· · · /				
).175 - 0.66	Low Noise	24	37	0.5	19	+5V @ 90 mA	LP3	EAR99	HMC616LP3E
0.23 - 0.66	Low Noise, Dual Channel	22	37	0.5	19	+5V @ 97 mA	LP4	EAR99	HMC816LP4E
0.3 - 3.0	Low Noise, High IP3	15	37	1.5	22	+5V @ 90 mA	SOT26	EAR99	HMC374E
0.55 - 1.2	Low Noise	16	37	0.5	21	+5V @ 88 mA	LP5	EAR99	HMC617LP3E
0.55 - 1.2	Low Noise, Dual Channel	16	37	0.5	20.5	+5V @ 95 mA	LP4	EAR99	HMC817LP4E
0.6 - 1.4	Low Noise	32	40	0.9	21.5	+5V @ 254 mA	LP4	EAR99	HMC718LP4E
0.7 - 1.2	Low Noise with Failsafe Bypass	16	33	0.9	13	+5V @ 57 mA	LP3	EAR99	HMC668LP3E
0.7 - 2.2	Low Noise	22	36	1.7	24	+5V @ 227 mA	LP3	EAR99	HMC758LP3E
1 - 11	Low Noise	17	30	1.5	18	+5V @ 55 mA	LP4	EAR99	HMC753LP4E
1 - 12	Low Noise	17	28	1.5	19	+5V @ 55 mA	Chip	EAR99	HMC-ALH444
1.2 - 3.0	Low Noise	26	21	1.3	11.5	+5V @ 21 mA	LP3	EAR99	HMC548LP3E
1.3 - 2.9	Low Noise	34	39	1	21.5	+5V @ 272 mA	LP4	EAR99	HMC719LP4E
1.7 - 2.2	Low Noise	19	36	0.75	20	+5V @ 117 mA	LP3	EAR99	HMC618LP3E
1.7 - 2.2	Low Noise with Failsafe Bypass	17	29	1.4	12	+5V @ 86 mA	LP3	EAR99	HMC669LP3E
1.7 - 2.2	Low Noise, Dual Channel	20.5	35	0.85	21	+5V @ 112 mA	LP4	EAR99	HMC818LP4E
2 - 4	Low Noise	10	36	2.6	21	+6V @ 100 mA	Chip	EAR99	HMC594 [1]
2 - 4	Low Noise	10	36	3	21	+6V @ 100 mA	LC3B	EAR99	HMC594LC3B
2 - 4	Low Noise	20.5	36	3	21	+6V @ 170 mA	Chip	EAR99	HMC609 [1]
2 - 4	Low Noise	20	36.5	3.5	21.5	+6V @ 170 mA	LC4	EAR99	HMC609LC4 [
2 - 12	Low Noise	15	25	1.8	13	+4V @ 45 mA	LC4	EAR99	HMC772LC4 [
2.1 - 2.9	Low Noise	19	33	0.9	19	+5V @ 95 mA	LP3	EAR99	HMC715LP3I
2.3 - 2.5	Low Noise	19	12	1.7	6	+3V @ 8.5 mA	SOT26	EAR99	HMC286E
2.3 - 2.7	Low Noise	19	29.5	0.75	16.5	+5V @ 59 mA	LP2	EAR99	HMC667LP2
2.3 - 2.7	Low Noise with Bypass	20	31	1.1	17	+5V @ 74 mA	LP3	EAR99	HMC605LP3
2.4 - 2.5	Transceiver, Front End	13	10	3	5	+3V @ 24 mA	MS8G	EAR99	HMC310MS80
3.1 - 3.9	Low Noise	18	33	1	19	+5V @ 65 mA	LP3	EAR99	HMC716LP3
3.3 - 3.8	Low Noise with Bypass	19	29	1.2	16	+5V @ 40 mA	LP3	EAR99	HMC593LP3
3.4 - 3.8	Low Noise with Bypass	16	18	2	7	+3V @ 9 mA	LP3	EAR99	HMC491LP3
3.5 - 7.0	Low Noise	15.5	28	2.4	16	+5V @ 50 mA	Chip	EAR99	HMC392
3.5 - 7.0	Low Noise	16	30	2.5	16	+5V @ 55 mA	LC4	EAR99	HMC392LC4
3.5 - 7.0	Low Noise	15	28	3	16	+5V @ 65 mA	LH5	EAR99	HMC392LH
4.8 - 6.0	Low Noise with Bypass	15	26	1.5	14	+5V @ 42 mA	LP3	EAR99	HMC604LP3
4.8 - 6.0	Low Noise	16.5	31.5	1.1	18.5	+5V @ 73 mA	LP3	EAR99	HMC717LP3
5 - 6	Low Noise	9	13	2.5	2	+3V @ 6 mA	MS8G	EAR99	HMC318MS80
5 - 6	Low Noise	12	10	2.5	9	+3V @ 25 mA	MS8G	EAR99	HMC320MS80
5 - 10	Low Noise	20	28	1.7	16	+3.5V @ 80 mA	Chip	EAR99	HMC902
5 - 10	Low Noise	19	28	1.8	16	+3.5V @ 80 mA	LP3	EAR99	HMC902LP3
5 - 20	Low Noise	13	26	2.2	16	+5V @ 30 mA	Chip	EAR99	HMC-ALH435
6 - 17	Low Noise	18	25	1.7	14	+3.5V @ 80 mA	LP3	EAR99	HMC903LP3
6 - 18	Low Noise	19	26	1.6	15	+3.5V @ 80 mA	Chip	EAR99	HMC903
6 - 20	Low Noise	22	20	2.3	10	+3V @ 53 mA	Chip	EAR99	HMC565
6 - 20	Low Noise	21	20	2.5	10	+3V @ 53 mA	LC5	EAR99	HMC565LC
6 - 26.5	Low Noise	22	18	2.5	10	+3.5V @ 45 mA	LC4	EAR99	HMC963LC4
7 - 13.5	Low Noise	17	24	1.8	12	+3V @ 51 mA	Chip	EAR99	HMC564
7 - 14	Low Noise	17	25	1.8	13	+3V @ 51 mA	LC4	EAR99	HMC564LC4
7 - 17 7.5 - 26.5	Low Noise	21	20	1.8	15	+3V @ 65 mA +3.5V @ 70 mA	Chip LC4	EAR99	HMC516 HMC962LC4
9 - 18	Low Noise	13 20		2.5	13		LC5	EAR99 EAR99	HMC516LC
	Low Noise  Medium Power LNA		25		14	+3V @ 65 mA			
12 - 16 12 - 17	Medium Power LNA	23	34 35	2.5	25 26	+5V @ 200 mA +5V @ 200 mA	LP5 Chip	EAR99 EAR99	HMC490LP5E HMC490 [1]
13 - 25	Low Noise	21	13	3.5	5	+3V @ 41 mA	Chip	EAR99	HMC342
13 - 25	Low Noise	22	20	3.5	9	+3V @ 41 mA	LC4	EAR99	
14 - 27	Low Noise	19.5	-	2.2	17	+4V @ 90 mA	LC4B	5A991.h	HMC342LC4
14 - 27	Low Noise	18.5		2.5	14	+4V @ 90 mA	Chip	5A991.h	HMC-ALH216
14 - 27	Low Noise	20	-	2.5	14	+4V @ 90 mA	Chip	5A991.h	HMC-ALH216
17 - 26	Low Noise	19	23	2.2	11	+3V @ 65 mA	Chip	EAR99	HMC517
17 - 26	Low Noise	19	23	2.5	13	+3V @ 65 mA	LC4	EAR99	HMC517LC4
17 - 26	Low Noise		25	2.2		+4V @ 73 mA	LC4	EAR99	HMC751LC4
18 - 31	Low Noise	25 15	23	3.5	13 11	+3V @ 75 mA	LC4	EAR99	HMC519LC4
18 - 32	Low Noise	15			12	+3V @ 75 mA		3A001.b.2.d	HMC519LC2
			23	2.8	14	AIII CO W VOT	Chip	JAUU 1.D.Z.U	HING 19



### SMT & Chip (Die) Products

Frequency	/ Function	Gain	OIP3	NF (dR)	P1dB	Bias	Package	ECCN	Part
(GHz) 20 - 32	Low Noise	( <b>dB</b> )	(dBm) 23	(dB) 3	(dBm) 12	+3V @ 65 mA	Chip	3A001.b.2.d	Number HMC518
21 - 29	Low Noise	13	19	2.5	8	+3V @ 65 mA +3V @ 35 mA	LC3B	EAR99	HMC518
22 - 26.5	Low Noise	25	-	3	12	+2.5V @ 52 mA	Chip	5A991.h	HMC-ALH311 [1]
24 - 28	Low Noise	25	26	2.5	13	+3V @ 70 mA	LC4	EAR99	HMC752LC4 [1]
24 - 30	Low Noise	13	16	2.5	6	+3V @ 30 mA	Chip	EAR99	HMC341
24 - 32	Low Noise	21	-	2	7	+5V @ 68 mA	Chip	3A001.b.2.d	HMC-ALH364
24 - 36	Low Noise	23	17	2	8	+3V @ 58 mA	Chip	3A001.b.2.d	HMC263
24 - 36	Low Noise	20	18	2.2	8	+3V @ 58 mA	LP4	3A001.b.2.d	HMC263LP4E
24 - 40	Low Noise	12	-	3.5	13	+4V @ 45 mA	Chip	3A001.b.2.d	HMC-ALH244
24 - 40	Low Noise	22	-	2	11	+5V @ 66 mA	Chip	3A001.b.2.d	HMC-ALH369
24 - 40	Low Noise	11.5	-	4	15	+4V @ 60 mA	Chip	3A001.b.2.d	HMC-ALH140 [1]
24 - 43.5	Low Noise	23	22	2.3	12	+2.5V @ 70 mA	LP3C	3A001.b.2.d	HMC1040LP3CE
27 - 33	Low Noise	20	-	3	12	+2.5V @ 52 mA	Chip	3A001.b.2.d	HMC-ALH313 [1]
28 - 36	Low Noise	21	24	2.8	12	+3V @ 82 mA	LP4	3A001.b.2.d	HMC566LP4E
29 - 36	Low Noise	20	23.5	2.8	12	+3V @ 80 mA	Chip	3A001.b.2.d	HMC566
35 - 45	Low Noise	16	-	2	6	+4V @ 87 mA	Chip	3A001.b.2.d	HMC-ALH376
37 - 42	Low Noise	22	-	3.5	12	+2.5V @ 52 mA	Chip	3A001.b.2.d	HMC-ALH310 [1]
57 - 65	Low Noise	21	-	4	12	+2.5V @ 64 mA	Chip	3A001.b.2.f	HMC-ALH382 [1]
71 - 86	Low Noise	13	-	5	7	+2.4V @ 30 mA	Chip	3A001.b.2.f	HMC-ALH508
71 - 86	Low Noise	14	-	5	7	+2V @ 50 mA	Chip	3A001.b.2.f	HMC-ALH509
Broadban	d Gain Blocks (Listed by P1dB Output P	ower)							
DC - 6	SiGe Gain Block	15.5	22	3	8	+5V @ 25 mA	MP86	EAR99	HMC474MP86E
DC - 6	SiGe Gain Block	15	20	3	8	+3V @ 25 mA	SC70	EAR99	HMC474SC70E
DC - 6	SiGe Gain Block	20	25	2.5	12	+5V @ 35 mA	MP86	EAR99	HMC476MP86E
DC - 6	SiGe Gain Block	19	24	2.5	12	+5V @ 35 mA	SC70	EAR99	HMC476SC70E
DC - 10	HBT Gain Block	15	24	4.5	13	+5V @ 56 mA	Chip	EAR99	HMC397
DC - 10	HBT Gain Block	15	25	4	13	+5V @ 50 mA	Chip	EAR99	HMC405
DC - 6	HBT Gain Block	17	27	6.5	14	+5V @ 50 mA	SOT26	EAR99	HMC313E
DC - 8	HBT Gain Block	12	30	6	14	+5V @ 56 mA	Chip	EAR99	HMC396
DC - 4	HBT Gain Block	15	28	4.5	15	+5V @ 54 mA	Chip	EAR99	HMC395
DC - 8	HBT Gain Block	15	30	5	15	+5V @ 54 mA	SC70	EAR99	HMC311SC70E
DC - 6	HBT Gain Block	14.5	32	4.5	15.5	+5V @ 56 mA	LP3	EAR99	HMC311LP3E
DC - 6	HBT Gain Block	16	31.5	4.5	15.5	+5V @ 54 mA	ST89	EAR99	HMC311ST89E
DC - 4	SiGe Gain Block	24	31	2.5	17	+5V @ 62 mA	SC70	EAR99	HMC478SC70E
DC - 4	SiGe Gain Block SiGe Gain Block	22	33	3	18	+5V @ 62 mA +5V @ 62 mA	MP86 ST89	EAR99	HMC478MP86E HMC478ST89E
DC - 4	SiGe Gain Block	15	34	4	18	+8V @ 72 mA	MP86	EAR99 EAR99	HMC479MP86E
DC - 5	SiGe Gain Block	15	34	4	18	+8V @ 75 mA	ST89	EAR99	HMC479NF80E
DC - 5	Dual SiGe Gain Block	15	34	4	18	+8V @ 75 mA	MS8G	EAR99	HMC469MS8GE
DC - 5	SiGe Gain Block	20	33	3.5	19	+8V @ 79 mA	ST89	EAR99	HMC481ST89E
DC - 10	pHEMT Gain Block	14	30	7	20	+5V @ 76 mA	LP2	EAR99	HMC788LP2E
DC - 5	SiGe Gain Block	19	34	2.9	20	+8V @ 82 mA	ST89	EAR99	HMC480ST89E
DC - 5	SiGe Gain Block	20	33	3.5	20	+8V @ 74 mA	MP86	EAR99	HMC481MP86E
DC - 5	Dual SiGe Gain Block	20	34	3.2	20	+8V @ 80 mA	MS8G	EAR99	HMC471MS8GE
DC - 4	HBT Gain Block	21	33	4	21	+5V @ 82 mA	ST89	EAR99	HMC589ST89E
0.2 - 4.0	Low Noise, High IP3, pHEMT Gain Block	13	38	2.3	22	+5V @ 110 mA	ST89	EAR99	HMC639ST89E
0.2 - 4.0	Low Noise, High IP3, pHEMT Gain Block	13	40	2.2	22	+5V @ 155 mA	ST89	EAR99	HMC636ST89E
DC - 1	HBT Gain Block	22	37	2.8	22	+5V @ 88 mA	ST89	EAR99	HMC580ST89E
DC - 4.5	HBT Gain Block	21	35	3.5	22	+8V @ 110 mA	ST89	EAR99	HMC475ST89E
DC - 5	SiGe Gain Block	19	36	4	22	+8V @ 110 mA	ST89	EAR99	HMC482ST89E
CATV Amp	olifiers								
0.04 - 0.96		5	27	3.5	12	+5V @ 120 mA	MS8G	EAR99	HMC549MS8GE
0.05 - 1.0	Low Noise, 75 Ohm	14	39	2.2	19	+5V @ 120 mA	ST89	EAR99	HMC599ST89E
0.04 - 1.0	50 / 75 Ohm Differential Gain Block	16	40	2.5	23.5	+5V @ 270 mA	LP4B	EAR99	HMC770LP4BE
0.05 - 3.0	HBT Gain Block	15	40	3.5	18	+5V @ 88 mA	ST89	EAR99	HMC740ST89E
0.05 - 3.0	HBT Gain Block	20	42	2.5	18.5	+5V @ 96 mA	ST89	EAR99	HMC741ST89E
DC - 1	HBT Gain Block, 75 Ohm	14	38	5.5	21	+5V @ 160 mA	S8G	EAR99	HMC754S8GE
Driver Am	plifiers								
0.7 - 2.8	HBT Driver Amplifier	18	42	3.8	25	+5V @ 125 mA	ST89	EAR99	HMC789ST89E
0.8 - 3.8	Driver Amplifier	18	30	7.5	17	+5V @ 53 mA	SOT26	EAR99	HMC308E
3.0 - 4.5	HBT Driver Amplifier	21	36	5	23.5	+5V @ 130 mA	MS8G	EAR99	HMC326MS8GE
17.5 - 41	Driver Amplifier	21	27	-	20	+5V @ 295 mA	Chip	3A001.b.2.d	HMC-AUH256



### SMT & Chip (Die) Products

Frequency (GHz)	Function	Gain (dB)	OIP3 (dBm)	NF (dB)	P1dB (dBm)	Bias Supply	Package	ECCN Code	Part Number
Linear & Pov	ver Amplifiers								
0.4 - 2.5	High IP3 Amp, 1/2 Watt	12.5	42	6	27	+5V @ 150 mA	ST89	EAR99	HMC454ST89
1.6 - 2.2	Medium Power Amplifier	22	40	5.5	27	+3.6V @ 270 mA	QS16G	EAR99	HMC413QS160
5 - 6	Medium Power Amplifier	17	38	6	26	+5V @ 300 mA	MS8G	EAR99	HMC406MS8G
5 - 7	Medium Power Amplifier	15	40	5.5	25	+5V @ 230 mA	MS8G	EAR99	HMC407MS8G
5 - 18	Medium Power Amplifier	18	28	7	19.5	+5V @ 120 mA	LP3	EAR99	HMC451LP3E
5 - 20	Medium Power Amplifier	22	30	6.5	20	+5V @ 127 mA	Chip	EAR99	HMC451
5 - 20	Medium Power Amplifier	19	30	7	19	+5V @ 114 mA	LC3	EAR99	HMC451LC3
6 - 18	Medium Power Amplifier	15.5	32	4.5	20	+5V @ 95 mA	Chip	EAR99	HMC441
6 - 18	<u></u>	17			20				HMC441LC3E
	Medium Power Amplifier		32	4.5		+5V @ 95 mA	LC3B	EAR99	
6.5 - 13.5	Medium Power Amplifier	14	29	4.5	18	+5V @ 95 mA	LP3	EAR99	HMC441LP3E
7 - 15.5	Medium Power Amplifier	15	32	4.8	20	+5V @ 95 mA	LH5 Hermetic	EAR99	HMC441LH5
7 - 15.5	Medium Power Amplifier	16	30	4.5	19	+5V @ 90 mA	LM1	EAR99	HMC441LM1
9.5 - 11.5	Medium Power Amplifier	29.5	33	6	27	+5V @ 310 mA	LC4	EAR99	HMC608LC4
12 - 30	Medium Power Amplifier	16	25	7	16	+5V @ 101 mA	Chip	EAR99	HMC383
12 - 30	Medium Power Amplifier	15	25	7.5	16.5	+5V @ 100 mA	LC4	EAR99	HMC383LC4
16 - 33	Medium Power Amplifier	17	33	-	24	+5V @ 400 mA	Chip	5A991.h	HMC-APH59
17 - 24	Medium Power Amplifier	24	34	4	25	+5V @ 250 mA	Chip	EAR99	HMC498
17 - 24	Medium Power Amplifier	22	36	4	25	+5V @ 250 mA	LC4	EAR99	HMC498LC4
17 - 30	Medium Power Amplifier	20	31	-	22	+4.5V @ 400 mA	Chip	5A991.h	HMC-APH19
17.5 - 24	Medium Power Amplifier	14	28	6.5	21.5	+5V @ 85 mA	LM1	EAR99	HMC442LM
17.5 - 25.5	Medium Power Amplifier	15	28	5.5	22	+5V @ 85 mA	Chip	EAR99	HMC442 [1]
17.5 - 25.5	Medium Power Amplifier	13	27	8	22	+5V @ 84 mA	LC3B	EAR99	HMC442LC3B
21 - 32	Medium Power Amplifier	16	33	5	24	+5V @ 200 mA	Chip	3A001.b.2.d	HMC499 [1]
21 - 32	Medium Power Amplifier	17	34	5	23	+5V @ 200 mA	LC4	3A001.b.2.d	HMC499LC4
! 33.5 - 46.5	Medium Power Amplifier, 0.5 Wattr	21	35	-	24.5	+6V @ 500 mA	Chip	3A001.b.2.d	HMC1014
34 - 42	Medium Power Amplifier	18.5	29	6.5	18	+5V @ 120 mA	Chip	3A001.b.2.d	HMC-ABH264
34 - 46.5	Medium Power Amplifier	22	34	-	24	+6V @ 250 mA	Chip	3A001.b.2.f	HMC1016
	· · · · · · · · · · · · · · · · · · ·						•		
37 - 40	Medium Power Amplifier	20	35		26	+5V @ 640 mA	Chip	3A001.b.2.d	HMC-APH51
37 - 45	Medium Power Amplifier	21	32	-	23	+5V @ 475 mA	Chip	3A001.b.2.d	HMC-APH40
50 - 66	Medium Power Amplifier	24	25	-	17	+5V @ 220 mA	Chip	3A001.b.2.f	HMC-ABH24
55 - 65	Medium Power Amplifier	13	25	-	16	+5V @ 80 mA	Chip	3A001.b.2.f	HMC-ABH209
71 - 76	Medium Power Amplifier	24	-	-	17.5	+4V @ 130 mA	Chip	3A001.b.2.f	HMC-AUH318
71 - 76	Medium Power Amplifier	13	-	-	20	+4V @ 240 mA	Chip	3A001.b.2.f	HMC-APH63
71 - 86	Medium Power Amplifier	15	-	-	15	+4V @ 130 mA	Chip	3A001.b.2.f	HMC-AUH320
81 - 86	Medium Power Amplifier	22	-	-	17.5	+4V @ 160 mA	Chip	3A001.b.2.f	HMC-AUH317
81 - 86	Medium Power Amplifier	12	-	-	19	+4V @ 240 mA	Chip	3A001.b.2.f	HMC-APH63
0.01 - 10	GaN Power Amplifier, 10 Watt	11	47	-	38	+48V @ 1100 mA	Chip	3A001.b.2.b	HMC999
0.1 - 22	Power Amplifier, 2 Watt	12	41	5	31	+15V @ 500 mA	Chip	3A001.b.2.c	HMC998
0.4 - 2.2	Power Amplifier, 1 Watt	21	49	6.5	30	+5V @ 510 mA	ST89	EAR99	HMC452ST8
0.4 - 2.2	Power Amplifier, 1.6 Watt	20.5	49	6.5	32	+5V @ 725 mA	ST89	EAR99	HMC453ST8
0.4 - 2.7	Power Amplifier, 2 Watt	16	48	8.5	33	+5V @ 700 mA	LP4	EAR99	HMC921LP4
0.45 - 2.2	Power Amplifier, 1 Watt	22.5	48	7	30	+5V @ 485 mA	QS16G	EAR99	HMC452QS16
0.45 - 2.2	Power Amplifier, 1.6 Watt	21.5	51	6.5	33	+5V @ 725 mA	QS16G	EAR99	HMC453QS16
DC - 32	Power Amplifier, 1/2 Watt	14	36	4	28	+10V @ 250 mA	Chip	EAR99	HMC994
1.7 - 2.2	Power Amplifier, 1 Watt	27	46	5	30.5	+5V @ 500 mA	QS16G	EAR99	HMC457QS16
2.3 - 2.8	Power Amplifier, 1 Watt	31	45	5	32.5	+5V @ 430 mA	LP4	EAR99	HMC755LP4
3 - 4	Power Amplifier, 1/2 Watt	21	40	5	27	+5V @ 250 mA	MS8G	EAR99	HMC327MS8
3.3 - 3.8	Power Amplifier, 1 Watt	31	45.5	5.8	30.5	+5V @ 615 mA	LP4	EAR99	HMC409LP4
5.1 - 5.9	Power Amplifier, 1 Watt	20	43	6	30	+5V @ 750 mA	LP3	EAR99	HMC408LP3
6 - 9.5	Power Amplifier, 1 Watt	21	40	-	30.5	+7V @ 820 mA	LP5	EAR99	HMC590LP5
6 - 9.5	Power Amplifier, 2 Watt	18	41	-	33	+7V @ 1340 mA	LP5	3A001.b.2.b	HMC591LP5
6 - 10	Power Amplifier, 1 Watt	25	41	-	31.5	+7V @ 820 mA	Chip	3A001.b.2.b	HMC590
6 - 10	Power Amplifier, 2 Watt	23	43	-	33.5	+7V @ 1340 mA	Chip	3A001.b.2.b	HMC591
7 - 9	Power Amplifier, 2 Watt	26	40	6.5	33.5	+7V @ 1.3A	Chip	3A001.b.2.b	HMC486
7 - 9	Power Amplifier, 2 Watt	22	40	7	32	+7V @ 1.3A	LP5	3A001.b.2.b	HMC486LP5
9 - 12	Power Amplifier, 2 Watt	20	36	8	32	+7V @ 1.3A	LP5	3A001.b.2.b	HMC487LP5
9 - 13.3	Power Amplifier, 2 Watt	34	42	5.5	33	+6V @ 1400 mA	Chip	3A001.b.2.b	HMC952
! 9-13.3	Power Amplifier, 2 Watt	33	43	-	34	+6V @ 1400 mA	LP5G	3A001.b.2.b	HMC952LP50
	•								
10 - 13	Power Amplifier, 1 West	19	38	-	31	+7V @ 750 mA	Chip	3A001.b.2.b	HMC592
	Power Amplifier, 1 Watt	13	34	9	31	+7V @ 1.3A	LP5	3A001.b.2.b	HMC489LP5
12 - 16 12.5 - 15.5	Power Amplifier, 2 Watt	30	42	-	34.5	+7V @ 1200 mA	Chip	3A001.b.2.b	HMC949



### SMT & Chip (Die) Products

Frequenc (GHz)	Function Function	Gain (dB)	OIP3 (dBm)	NF (dB)	P1dB (dBm)	Bias Supply	Package	ECCN Code	Part Number
12.5 - 15.	5 Power Amplifier, 4 Watt	28	44	-	36	+7V @ 1200 mA	Chip	3A001.b.2.b	HMC950
12.5 - 15.	5 Power Amplifier, 2 Watt	27	40	-	32	+6V @ 1200 mA	LP5	3A001.b.2.b	HMC965LP5E
12 - 16	PA with Power Detector, 3 Watt	27	41	-	34.5	+7V @ 1200 mA	LP5G	3A001.b.2.b	HMC995LP5G
15 - 27	Power Amplifier, 1 Watt	17	37	-	29	+5V @ 1.44A	Chip	3A001.b.2.c	HMC-APH462
16 - 24	Power Amplifier, 1 Watt	23	41	-	31	+7V @ 790 mA	Chip	3A001.b.2.c	HMC756
16 - 24	Power Amplifier, 1/2 Watt	22	37	-	29	+7V @ 395 mA	Chip	EAR99	HMC757
16 - 24	Power Amplifier, 1/2 Watt	20.5	34.5	-	26.5	+5V @ 400 mA	LP4	EAR99	HMC757LP4E
18 - 20	Power Amplifier, 1 Watt	17.5	38.5	-	30	+5V @ 900 mA	Chip	3A001.b.2.c	HMC-APH478
21 - 24	Power Amplifier, 1 Watt	17	39	-	30.5	+5V @ 950 mA	Chip	3A001.b.2.c	HMC-APH518
22 - 26.5	5 Power Amplifier, 1/2 Watt	20	33	7	26.5	+5V @ 400 mA	LP4	EAR99	HMC863LP4I
22.5 - 26.	· · · · · · · · · · · · · · · · · · ·	17	40	-	30	+5V @ 950 mA	Chip	3A001.b.2.c	HMC-APH60
24 - 29.5		22	-	-	26.5	+6V @ 360 mA	Chip	EAR99	HMC863
24 - 29.5	· · · · · · · · · · · · · · · · · · ·	27	40	-	29	+6V @ 750 mA	Chip	3A001.b.2.c	HMC864
24 - 31.5	•	22	43		34	+5.5V @ 1200 mA	LP5	3A001.b.2.c	HMC943LP5
27 - 31.5		14	37	_	28	+5V @ 900 mA	Chip	3A001.b.2.c	HMC-APH46
27 - 34	Power Amplifier, 1 Watt	17.5	37		29	+5V @ 800 mA	Chip	3A001.b.2.d	HMC693
27.3 - 33.	•	23	43		33	+6V @ 1200 mA	Chip	3A001.b.2.d	HMC906
! 27.5 - 33.	•	24	40		29	+6V @ 600 mA	Chip	3A001.b.2.d	HMC1024
! 29 - 37	Power Amplifier, 2 Watt	22	42	6	32	+6V @ 1200 mA	Chip	3A001.b.2.d	HMC1029
37 - 40	Power Amplifier, 1 Watt	15	37	-	28	+5V @ 1.08A	Chip	3A001.b.2.d	HMC-APH47
	. ,	21						3A001.b.2.d	
37 - 40	Power Amplifier, 1 Watt	22	38	-	30.5	+6V @ 900 mA	Chip		HMC968
40 - 43.5		22	38		29	+6V @ 900 mA	Chip	EAR99	HMC969
	d (Distributed) Amplifiers								
DC - 20		14	28	2.5	16	+8V @ 60 mA	Chip	EAR99	HMC460 [1]
DC - 20		14	29.5	2.5	17	+8V @ 75 mA	LC5	EAR99	HMC460LC5
2 - 20	Wideband LNA	15	26.5	2.5	15	+5V @ 63 mA	Chip	EAR99	HMC462
2 - 20	Wideband LNA	13	25	2.5	14	+5V @ 66 mA	LP5	EAR99	HMC462LP5
2 - 20	Wideband LNA with AGC	14	28	2.5	19	+5V @ 60 mA	Chip	EAR99	HMC463 [1]
2 - 20	Wideband LNA with AGC	13	26	3	18	+5V @ 60 mA	LP5	EAR99	HMC463LP5E
2 - 20	Wideband LNA with AGC	14	28	2.5	18	+5V @ 60 mA	LH250	EAR99	HMC463LH25
2 - 20	Wideband LNA	10	-	3.5	10	+2V @ 55 mA	Chip	EAR99	HMC-ALH10
2 - 22	Wideband LNA	16	-	1.7	14	+4V @ 45 mA	Chip	EAR99	HMC-ALH48
DC - 20	Wideband Driver	17	30	2.5	22	+8V @ 160 mA	Chip	EAR99	HMC465 [1]
DC - 20	Wideband Driver	15	28	3	23	+8V @ 160 mA	LP5	EAR99	HMC465LP5E
DC - 35	Wideband Driver	15	-	-	21	+5V @ 200 mA	Chip	3A001.b.2.d	HMC-AUH24
DC - 43	Wideband Driver	14	-	5.4	16.5	+5V @ 180 mA	Chip	3A001.b.2.d	HMC-AUH23
0.5 - 65	Wideband Driver	10	-	-	-	+8V @ 60 mA	Chip	3A001.b.2.d	HMC-AUH31
2 - 35	Wideband Driver	12.5	27	3	18	+8V @ 80 mA	Chip	3A001.b.2.d	HMC562 [1]
5 - 17	Wideband Driver	31	30	8	23	+5V @ 180 mA	Chip	EAR99	HMC633 [1]
5 - 20	Wideband Driver	22	31	7.5	23	+5V @ 180 mA	Chip	EAR99	HMC634 [1]
5 - 20	Wideband Driver	21	29	7.5	22	+5V @ 180 mA	LC4	EAR99	HMC634LC4
5.5 - 17	Wideband Driver	30	30	8	23	+5V @ 180 mA	LC4	EAR99	HMC633LC4
18 - 40	Wideband Driver	19.5	29	8	23	+5V @ 280 mA	Chip	3A001.b.2.e	HMC635
18 - 40	Wideband Driver	18.5	27	7	22	+5V @ 280 mA	LC4	3A001.b.2.d	HMC635LC4
DC - 48		12	32	-	22	+10V @ 150 mA	Chip	3A001.b.2.f	HMC1022
DC - 6	Wideband Power Amplifier	14	45	5	29	+12V @ 400 mA	Chip	EAR99	HMC637
DC - 6	Wideband Power Amplifier	13	40	5	29	+12V @ 400 mA	LP5	EAR99	HMC637LP5
DC - 10	<u>'</u>	12	41	6	28.5	+12V @ 400 mA	Chip	EAR99	HMC619
	· · · · · · · · · · · · · · · · · · ·				28		LP5		
DC - 15		12	41	6		+12V @ 300 mA +8V @ 300 mA		EAR99	HMC619LP5
DC - 15	· · · · · · · · · · · · · · · · · · ·	19	35	2	26.5		Chip	EAR99	HMC659
DC - 15	<u>'</u>	19	35	2.5	27.5	+8V @ 300 mA	LC5	EAR99	HMC659LC
DC - 18	· · · · · · · · · · · · · · · · · · ·	17	32	3	25	+8V @ 290 mA	Chip	EAR99	HMC459
DC - 20	· · · · · · · · · · · · · · · · · · ·	14	36	4	28	+10V @ 400 mA	Chip	3A001.b.2.c	HMC559
DC - 22	· · · · · · · · · · · · · · · · · · ·	14	40	2.5	28	+11V @ 400 mA	Chip	3A001.b.2.c	HMC797
DC - 22	· · · · · · · · · · · · · · · · · · ·	13.5	39	4	28	+10V @ 400 mA	LP5	EAR99	HMC797LP5
DC - 40		13	33.5	5	22	+10V @ 175 mA	Chip	3A001.b.2.d	HMC930 [1]
0.2 - 22	Wideband Power Amplifier	13	38	3	27	+11V @ 365 mA	Chip	EAR99	HMC907
0.2 - 22	Wideband Power Amplifier	12	36	3.5	26	+10V @ 350 mA	LP5	EAR99	HMC907LP5



### SMT & Chip (Die) Products

### **AMPLIFIERS**

Frequency (GHz)	Function	Gain (dB)	OIP3 (dBm)	NF (dB)	P1dB (dBm)	Bias Supply	Package	ECCN Code	Part Number
2 - 20	Wideband Power Amplifier	16	30	4	26	+8V @ 290 mA	Chip	EAR99	HMC464
2 - 20	Wideband Power Amplifier	14	30	4	26	+8V @ 290 mA	LP5	EAR99	HMC464LP5E

[1] Amplifiers that benefit from Hittite Active Bias Controllers

### **AMPLIFIERS** - Low Phase Noise

Frequency (GHz)	Function	Gain / NF (dB)	OIP3 (dBm)	10 kHz SSB Phase Noise (dBc/Hz)	P1dB / Psat (dBm)	Bias Supply	Package	ECCN Code	Part Number
2 - 18	Wideband, Low Phase Noise	14 / 4.5	27	-160	15 / 18	+5V @ 64 mA	Chip	EAR99	HMC606
2 - 18	Wideband, Low Phase Noise	13.5 / 5	27	-160	15 / 17	+5V @ 64 mA	LC5	EAR99	HMC606LC5

### **ATTENUATORS**

Frequency (GHz)	Function	Insertion Loss (dB)	Attenuation Range (dB)	IIP3 (dBm)	Control Input (Vdc)	Package	ECCN Code	Part Number
Attenuators -	· Analog		mango (az)	(4.2)	mput (vuo)			Trainizo.
0.45 - 2.2	Analog VVA	1.9	0 to 48	20	0 to +3V	MS8	EAR99	HMC473MS8E
0.5 - 6.0	Analog VVA	2.5	0 to 26	35	0 to +5V	LP3	EAR99	HMC973LP3E
DC - 8	Analog VVA	1.5	0 to 32	10	0 to -3V	MS8G	EAR99	HMC346MS8GE
DC - 8	Analog VVA	2	0 to 30	10	0 to -3V	C8	EAR99	HMC346C8
DC - 8	Analog VVA	2	0 to 30	10	0 to -3V	G8 Hermetic	EAR99	HMC346G8
DC - 14	Analog VVA	2	0 to 30	10	0 to -3V	LP3	EAR99	HMC346LP3E
DC - 18	Analog VVA	1.5	0 to 30	10	0 to -3V	LC3B	EAR99	HMC346LC3B
DC - 20	Analog VVA	2.2	0 to 25	10	0 to -3V	Chip	EAR99	HMC346
5 - 26.5	Analog VVA	3.5	0 to 28	32	0 to -3V	LP3C	EAR99	HMC712LP3CE
5 - 30	Analog VVA	2.5	0 to 30	32	0 to -3V	Chip	EAR99	HMC712
5 - 30	Analog VVA	2	0 to 28	28	0 to -3V	LC4	EAR99	HMC812LC4
17 - 27	Analog VVA	1.5	0 to 22	17	-4 to +4V	Chip	5A991.h	HMC-VVD102
20 - 50	Analog VVA	3	0 to 35	33	0 to +3V	Chip	EAR99	HMC985
36 - 50	Analog VVA	1.5	0 to 22	17	0 to +4V	Chip	5A991.h	HMC-VVD106
70 - 86	Analog VVA	2	0 to 14	-	-5 to +5V	Chip	5A991.h	HMC-VVD104
Attenuators -								
DC - 5	1-Bit Digital	1	10	50	TTL/CMOS	LP3	EAR99	HMC541LP3E
DC - 10	1-Bit Digital	2	10	54	0 / +3 to +5V	LP3	EAR99	HMC800LP3E
DC - 10	1-Bit Digital	1.5	15	53	0 / +3 to +5V	LP3	EAR99	HMC801LP3E
DC - 10	1-Bit Digital	2.5	20	53	0 / +3 to +5V	LP3	EAR99	HMC802LP3E
0.7 - 4.0	2-Bit Digital	0.5	2 to 6	52	0 / +3V	SOT26	EAR99	HMC290E
0.7 - 4.0	2-Bit Digital	0.9	4 to 12	54	0 / +3V	SOT26	EAR99	HMC291E
DC - 6	2-Bit Digital	0.5	2 to 6	50	TTL/CMOS	LP3	EAR99	HMC467LP3E
0.75 - 2.0	3-Bit Digital	1.8	4 to 28	45	0 / +3V	MS8	EAR99	HMC230MS8E
0.7 - 3.7	3-Bit Digital	1.3	2 to 14	51	0 / +3V	MS8	EAR99	HMC288MS8E
DC - 6	3-Bit Digital	0.7	1 to 7	50	TTL/CMOS	LP3	EAR99	HMC468LP3E
DC - 5.5	4-Bit Digital	0.8	1 to 15	50	TTL/CMOS	LP3	EAR99	HMC540LP3E
DC - 6	4-Bit Digital, Serial & Parallel Control	2.5	3 to 45	50	0 / +5V	LP4	EAR99	HMC629LP4E
0.1 - 30	5-Bit Digital	2.5	0.5 to 15.5	45	0 / +3 to +5V	Chip	EAR99	HMC941
0.1 - 30	5-Bit Digital, Serial Control	5	1 to 31	43	0 / +3 to +5V	LP4	EAR99	HMC1018LP4E
0.1 - 30	5-Bit Digital, Serial Control	4	0.5 to 15.5	45	0 / +3 to +5V	LP4	EAR99	HMC1019LP4E
0.1 - 33	5-Bit Digital	5	1 to 31	43	0 / +3 to +5V	LP4	EAR99	HMC939LP4E
0.1 - 33	5-Bit Digital	4	0.5 to 15.5	45	0 / +3 to +5V	LP4	EAR99	HMC941LP4E
0.1 - 33		3.5	1 to 31	43	0 / +3 to +5V	Chip	EAR99	HMC939
0.7 - 2.7	5-Bit Digital	2.3	1 to 31	54	0/+3t0+3V	QS16	EAR99	HMC274QS16E
0.7 - 2.7	5-Bit Digital 5-Bit Digital, Serial Control	2.3	1 to 31	48	Serial/CMOS	LP4	EAR99	HMC271ALP4E
0.7 - 3.8		2.1	1 to 31	48	0 / +3V	MS10G	EAR99	
0.7 - 3.8	5-Bit Digital 5-Bit Digital, Serial Control	1.5	0.5 to 15.5	52	Serial/CMOS	LP4	EAR99	HMC273MS10GE HMC305ALP4E
0.7 - 3.8		1.5		52	0 / +3V	MS10	EAR99	
	5-Bit Digital	1.3	0.5 to 15.5			MS10 MS10		HMC306MS10E
0.7 - 3.8	5-Bit Digital	1.3	0.5 to 15.5	48	0 / +3V 0 / +3V		EAR99 EAR99	HMC603MS10E
	5-Bit Digital		0.5 to 15.5	48		QS16		HMC603QS16E
DC - 3	5-Bit Digital	2.0	1 to 31	44	0 / -5V	G16 Hermetic	EAR99	HMC335G16
DC - 3	5-Bit Digital	1.3	1 to 31	45	TTL/CMOS	LP3	EAR99	HMC470LP3E
DC - 4	5-Bit Digital	1.9	1 to 31	44	0 / -5V	QS16G	EAR99	HMC307QS16GE
DC - 4	5-Bit Digital	0.7	0.25 to 7.75	50	TTL/CMOS	LP3	EAR99	HMC539LP3E
0.06 - 0.5	6-Bit Digital, Serial & Parallel Control	1.2	0.5 to 31.5	55	0 / +3 to +5V	LP4	EAR99	HMC624LFLP4E



### SMT & Chip (Die) Products

### **ATTENUATORS**

Frequency (GHz)	Function	Insertion Loss (dB)	Attenuation Range (dB)	IIP3 (dBm)	Control Input (Vdc)	Package	ECCN Code	Part Number
DC - 3.8	6-Bit Digital	1.5	0.5 to 31.5	45	TTL/CMOS	LP4	EAR99	HMC472LP4E
DC - 3	6-Bit Digital	3.0	0.5 to 31.5	32	0 / -5V	G16 Hermetic	EAR99	HMC424G16
DC - 4	6-Bit Digital, Serial Control	1.2	0.5 to 31.5	45	Serial/CMOS	LP4	EAR99	HMC542ALP4E
DC - 6	6-Bit Digital, Serial & Parallel Control	1.8	0.5 to 31.5	55	0 / +5V	LP4	EAR99	HMC624LP4E
DC - 6	6-Bit Digital, Serial & Parallel Control	1.8	0.25 to 15.75	55	TTL/CMOS	LP4	EAR99	HMC792LP4E
DC - 13	6-Bit Digital	4.0	0.5 to 31.5	32	0 / -5V	Chip	EAR99	HMC424
DC - 13	6-Bit Digital	3.2	0.5 to 31.5	32	0 / -5V	LH5 Hermetic	EAR99	HMC424LH5
DC - 13	6-Bit Digital	4.0	0.5 to 31.5	32	0 / -5V	LP3	EAR99	HMC424LP3E
2.4 - 8.0	6-Bit Digital	3.5	0.5 to 31.5	40	0 / +5V	Chip	EAR99	HMC425
2.2 - 8.0	6-Bit Digital	3.2	0.5 to 31.5	40	0 / +5V	LP3	EAR99	HMC425LP3E
0.01 - 0.3	7-Bit Digital	3.3	0.25 to 31.75	40	TTL/CMOS	LP3	EAR99	HMC759LP3E

### **AUTOMATIC GAIN CONTROL**

Frequency (MHz)	Function	Gain Control Range (dB)	NF (dB)	OIP3 (dBm)	P1dB (dBm)	Bias Supply	Package	ECCN Code	Part Number
50 - 800	IF Automatic Gain Controller	-10 to +38	6	40	19	+5V @ 215 mA	LP5	EAR99	HMC992LP5E
700 - 3000	RF Automatic Gain Controller	-11 to +32	7.6	46	25	+5V @ 260 mA	LP5	EAR99	HMC993LP5E

### DC POWER CONDITIONING - Linear Voltage Regulators

Input Voltage (	V) Function	Output Voltage (V)	Output Current (mA)		oly Rejection SRR) (dB) 1 MHz		se Spectral (nV/√Hz) 10 kHz	Regulated Outputs	Package	ECCN Code	Part Number
3.35 - 5.	6 Quad High PSRR	2.5 - 5.2	15 - 100	80	60	7	3	4	LP3	EAR99	HMC860LP3E
3.35 - 5.	6 Low Noise, High PSRR	1.8 - 5.2	500	80	60	7	3	4	LP3	EAR99	HMC1060LP3E
4.8 to 5.	6 Low Noise, High PSRR	1.8 to 5.1	400	60	30	6	3	1	LP3	EAR99	HMC976LP3E

### FILTERS - Tunable

### Programmable Harmonic

	Frequency Range (GHz)	Function	Return Loss (dB)	3 dB Bandwidth (GHz)	Stopband Frequency (Rej. >10 dB)	Tuning Response (ns)	Package	ECCN Code	Part Number
NEW!	0.25 - 3.025	Programmable Harmonic Low Pass	10	1 - 3	1.2 Fcutoff	10	LP3	EAR99	HMC1044LP3E

### **Band Pass**

	Frequency Range (GHz)	Function	Return Loss (dB)	3 dB Bandwidth (%)	Low Side Rejection Frequency (Rej. >20 dB)	High Side Rejection Frequency (Rej. >20 dB)	Tuning Response (ns)	Package	ECCN Code	Part Number
_	1 - 2	Band Pass	10	11	0.8 x Fcenter	1.2 x Fcenter	200	LP5	EAR99	HMC890LP5E
_	2 - 3.9	Band Pass	10	9	0.9 x Fcenter	1.15 x Fcenter	200	LP5	EAR99	HMC891LP5E
	4 - 7.7	Band Pass	15	9	0.9 x Fcenter	1.13 x Fcenter	200	LP5	EAR99	HMC892LP5E
	4.8 - 9.5	Band Pass	7	6.5	0.9 x Fcenter	1.1 x Fcenter	200	LP5	EAR99	HMC893LP5E
_	5.9 - 11.2	Band Pass	7.5	6	0.92 x Fcenter	1.08 x Fcenter	200	LP5	EAR99	HMC894LP5E
	6.8 - 12.6	Band Pass	12	10	0.88 x Fcenter	1.1 x Fcenter	200	LP4	EAR99	HMC895LP4E
IEW!	9 - 19	Band Pass	9.5	18	0.81 x Fcenter	1.17 x Fcenter	200	Chip	EAR99	HMC897
	9 - 19	Band Pass	9.5	18	0.81 x Fcenter	1.17 x Fcenter	200	LP4	EAR99	HMC897LP4E
	10 - 18	Band Pass	11	9	0.89 x Fcenter	1.1 x Fcenter	200	LP4	EAR99	HMC896LP4E
	11.5 - 21.5	Band Pass	9	17	0.81 x Fcenter	1.16 x Fcenter	200	LP4	EAR99	HMC898LP4E
	18.5 - 37.0	Band Pass	10	18	0.81 x Fcenter	1.20 x Fcenter	200	LP4	EAR99	HMC899LP4E
	19 - 38	Band Pass	10	18	0.81 x Fcenter	1.20 x Fcenter	< 100	Chip	EAR99	HMC899

### Low Pass

Frequency Range (GHz)	Function	Return Loss (dB)	Cutoff Frequency Range (GHz)	Stopband Frequency (Rej. >20 dB)	Tuning Response (ns)	Package	ECCN Code	Part Number
DC - 4.0	Low Pass	10	2.2 - 4.0	1.25 x Fcutoff	150	LP5	EAR99	HMC881LP5E
DC - 7.6	Low Pass	10	4.5 - 7.6	1.23 x Fcutoff	150	LP5	EAR99	HMC882LP5E

### **Band Reject**

Frequency Range (GHz)	Function	Rejection Band Tuning Freq. (GHz)	Pass Band Insertion Loss (dB)	Stop Band Rejection (dB)	20 dB Bandwidth (%)	Tuning Response (ns)	Package	ECCN Code	Part Number
0.1 - 25	Band Reject	3.6 - 12.2	3	25	8	200	LP5	EAR99	HMC1000LP5E



### **SMT & Chip (Die) Products**

### IF / BASEBAND PROCESSING - Dual Baseband Low Pass Filter & Dual Baseband Digital VGA

### **Dual Baseband Low Pass Filter**

3.5 - 50 Dual Low Pass with ADC Driver ± 2.5 0 / 10 12 30 LP5 EAR99 HMC900LP5E	3 dB Bandwidth Setting (MHz)	Function	3 dB Bandwidth Accuracy (%)	Gain (dB)	NF (dB)	OIP3 (dBm)	Package	ECCN Code	Part Number
	3.5 - 50	Dual Low Pass with ADC Driver	± 2.5	0 / 10	12	30	LP5	EAR99	HMC900LP5E

Please Note: 400 Ohm Reference Impedance Are Shown

### **Dual Baseband Digital VGA**

Frequency (MHz)	Function	NF (dB)	Variable Gain (dB)	OIP3 (dBm)		Sideband Supp. (dB)	Magnitude (dB) / Phase (deg) Balance	Bias Supply	Package	ECCN Code	Part Number
DC - 100	Digital, Serial & Parallel Control	6	0 to 40	+30	+65	55	±0.1 / ±1	+5V @ 70 mA	LP4	EAR99	HMC960LP4E

Please Note: 100 Ohm Reference Impedance Are Shown

### I/Q MIXERS / IRMs

RF Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	Image Rejection (dB)	IIP3 (dBm)	Package	ECCN Code	Part Number
3 - 7	I/Q Mixer / IRM	DC - 3.5	-7.5	33	23	Chip	EAR99	HMC620
3 - 7	I/Q Mixer / IRM	DC - 3.5	-7.5	32	22	LC4	EAR99	HMC620LC4
4 - 8.5	I/Q Mixer / IRM	DC - 3.5	-7.5	40	23	Chip	EAR99	HMC525
4 - 8.5	I/Q Mixer / IRM	DC - 3.5	-7.5	40	23	LC4	EAR99	HMC525LC4
5.9 - 12.0	I/Q Mixer / IRM	DC - 1.5	-8	30	18	Chip	EAR99	HMC256
6 - 10	I/Q Mixer / IRM	DC - 3.5	-7	40	22	Chip	EAR99	HMC520
6 - 10	I/Q Mixer / IRM	DC - 3.5	-7	40	23	LC4	EAR99	HMC520LC4
6 - 10	I/Q Mixer / IRM	DC - 3.5	-7.5	40	28	Chip	EAR99	HMC526
6 - 10	I/Q Mixer / IRM	DC - 3.5	-7.5	40	28	LC4	EAR99	HMC526LC4
8.5 - 13.5	I/Q Mixer / IRM	DC - 3.5	-7.5	40	24	Chip	EAR99	HMC521
8.5 - 13.5	I/Q Mixer / IRM	DC - 3.5	-7.5	38	24	LC4	EAR99	HMC521LC4
8.5 - 13.5	I/Q Mixer / IRM	DC - 2	-7.5	35	28	Chip	EAR99	HMC527
8.5 - 13.5	I/Q Mixer / IRM	DC - 2	-7.5	34	28	LC4	EAR99	HMC527LC4
10 - 16	I/Q Mixer / IRM	DC - 3.5	-8	25	25	LC5	EAR99	HMC775LC5
11 - 16	I/Q Mixer / IRM	DC - 3.5	-7.5	35	24	Chip	EAR99	HMC522
11 - 16	I/Q Mixer / IRM	DC - 3.5	-7.5	35	24	LC4	EAR99	HMC522LC4
11 - 16	I/Q Mixer / IRM	DC - 3.5	-8	35	27	Chip	EAR99	HMC528
11 - 16	I/Q Mixer / IRM	DC - 3.5	-8	35	26	LC4	EAR99	HMC528LC4
15 - 23	I/Q Mixer / IRM	DC - 3.5	-8	25	25	LC4	EAR99	HMC523LC4
15 - 23.6	I/Q Mixer / IRM	DC - 3.5	-8	27	25	Chip	EAR99	HMC523
<b>W!</b> 15 - 33.5	I/Q Mixer / IRM	DC - 3.5	-10	40	22	LC4	EAR99	HMC1042LC4
17 - 27	I/Q Mixer / IRM	DC - 3.5	-9	36	20	LC4	EAR99	HMC1041LC4
19 - 33	I/Q Mixer / IRM	DC - 5	-8	25	17	Chip	5A001.h	HMC-MDB172
22 - 32	I/Q Mixer / IRM	DC - 3.5	-10	23	20	Chip	EAR99	HMC524
22 - 32	I/Q Mixer / IRM	DC - 4.5	-10	20	20	LC3B	EAR99	HMC524LC3B
15 - 33.5	I/Q Mixer / IRM	DC - 3.5	-10	30	22	LC4	EAR99	HMC1042LC4
31 - 38	I/Q Mixer / IRM	DC - 3.5	-10.5	17	21	Chip	EAR99	HMC555
35 - 45	I/Q Mixer / IRM	DC - 5	-8	25	17	Chip	5A991.h	HMC-MDB171
36 - 41	I/Q Mixer / IRM	DC - 3.5	-11	18	23	Chip	EAR99	HMC556
55 - 64	I/Q Mixer / IRM	DC - 3	-9	30	16	Chip	5A991.h	HMC-MDB207
26 - 33 RF	Sub-Harmonic, I/Q Mixer / IRM	DC - 3	-11	22	16	Chip	EAR99	HMC404
54 - 64 RF	Sub-Harmonic, I/Q Mixer / IRM	DC - 3	-12.5	30	7	Chip	5A991.h	HMC-MDB218

### I/Q DOWNCONVERTER / RECEIVERS

RF Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	Noise Figure (dB)	Image Rejection (dB)	IIP3 (dBm)	Package	ECCN Code	Part Number
5.6 - 8.6	I/Q Downconverter / Receiver	DC - 3	12	2.2	20	2	LP4	EAR99	HMC951LP4E
7 - 9	I/Q Downconverter / Receiver	DC - 3.5	10	2.5	35	1.5	LC5	EAR99	HMC567LC5
9 - 12	I/Q Downconverter / Receiver	DC - 3.5	11	2.2	25	2	LC5	EAR99	HMC908LC5
12 - 16	I/Q Downconverter / Receiver	DC - 3.5	14	2.8	32	-1	LC5	EAR99	HMC869LC5
17 - 20	I/Q Downconverter / Receiver	DC - 3.5	14	2.5	40	0	LP4	EAR99	HMC966LP4E
17 - 21	I/Q Downconverter / Receiver	DC - 3.5	10	3	17	3	Chip	EAR99	HMC570
17 - 21	I/Q Downconverter / Receiver	DC - 3.5	10	3	18	2	LC5	EAR99	HMC570LC5
17 - 24	I/Q Downconverter / Receiver	DC - 3.3	11	2.2	21	2	LC5	EAR99	HMC904LC5
17 - 24	I/Q Downconverter / Receiver	DC - 3.5	15	2.5	25	1	LP4	EAR99	HMC967LP4E
20 - 28	I/Q Downconverter / Receiver	DC - 3.5	14	2.5	21	1	LP4	EAR99	HMC977LP4E
21 - 25	I/Q Downconverter / Receiver	DC - 3.5	11	3	24	5	Chip	EAR99	HMC571
21 - 25	I/Q Downconverter / Receiver	DC - 3.5	10	2	20	5	LC5	EAR99	HMC571LC5
24 - 28	I/Q Downconverter / Receiver	DC - 3.5	8	3.5	20	5	Chip	EAR99	HMC572
24 - 28	I/Q Downconverter / Receiver	DC - 3.5	8	3.5	18	5	LC5	EAR99	HMC572LC5



### SMT & Chip (Die) Products

### I/Q UPCONVERTER / TRANSMITTERS

RF Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	Sideband Rejection (dBc)	OIP3 (dBm)	Package	ECCN Code	Part Number
5.5 - 8.6	I/Q Upconverter / Transmitter w/ VGA	DC - 3	16.5	-30	29	LC5	EAR99	HMC925LC5
10 - 16	I/Q Upconverter / Transmitter w/ VGA	DC - 3	17	-30	14	LC5	EAR99	HMC924LC5
11 - 17	I/Q Upconverter / Transmitter	DC - 2	13	-20	26	LC5	EAR99	HMC709LC5
16 - 21	I/Q Upconverter / Transmitter	DC - 3.5	12	-20	30	LC5	EAR99	HMC710LC5
17.7 - 23.6	I/Q Upconverter / Transmitter	DC - 3.5	15	-35	35	LC5	EAR99	HMC819LC5
21 - 27	I/Q Upconverter / Transmitter	DC - 3.75	12	-20	27	LC5	EAR99	HMC815LC5

#### MIXERS

RF Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	LO / RF Isolation (dB)	IIP3 (dBm)	Package	ECCN Code	Part Number
igh IP3 Mixer	s							
0.4 - 0.65	High IP3, 0 LO	DC - 0.25	-9	7	33	MS8G	EAR99	HMC585MS8
0.45 - 0.5	High IP3, SGL-END	DC - 0.15	-9.5	20	32	MS8	EAR99	HMC387MS
0.5 - 2.7	High IP3, DBL-BAL, +2 LO	DC - 1	-8	28	28	LP4	EAR99	HMC915LP4
0.7 - 1.0	High IP3, SGL-END	DC - 0.25	-8.5	24	35	MS8	EAR99	HMC399MS
0.7 - 1.0	High IP3, DBL-BAL, 0 LO	DC - 0.45	-7	23	32	LP4	EAR99	HMC684LP
0.7 - 1.1	High IP3, DBL-BAL, 0 LO	0.05 - 0.25	-7.5	24	40	LP4	EAR99	HMC786LF
0.7 - 1.2	High IP3, DBL-BAL	DC - 0.3	-9	42	25	S8	EAR99	HMC351S8
0.7 - 1.5	High IP3, 0 LO	DC - 0.35	-9	20	33	MS8G	EAR99	HMC483MS
0.7 - 1.5	High IP3, DBL-BAL, 0 LO	DC - 0.5	-7.5	24	34	LP4	EAR99	HMC686LP
0.8 - 1.2	High IP3, DBL-BAL, 0 LO	DC - 0.3	-8	27	27	LP4	EAR99	HMC551LP
1.5 - 3.5	High IP3, DBL-BAL	DC - 1	-8	38	25	MS8	EAR99	HMC316MS
1.6 - 3.0	High IP3, DBL-BAL, 0 LO	DC - 1	-8	30	25	LP4	EAR99	HMC552LP
1.7 - 2.2	High IP3, SGL-END	DC - 0.3	-8.8	30	36	MS8	EAR99	HMC400MS
1.7 - 2.2	High IP3, DBL-BAL, 0 LO	DC - 0.5	-8	30	35	LP4	EAR99	HMC685LP
1.7 - 2.2	High IP3, DBL-BAL, 0 LO	DC - 0.5	-8	31	34	LP4	EAR99	HMC687LP
1.7 - 2.2	High IP3, DBL-BAL, 0 LO	0.05 - 0.30	-8	30	38	LP4	EAR99	HMC785LP
1.7 - 2.4	High IP3, SGL-END	0.05 - 0.3	-9.2	10	34	MS8G	EAR99	HMC485MS
1.7 - 3.0	High IP3, SGL-BAL	DC - 0.8	-9	30	30	MS8	EAR99	HMC304MS
1.7 - 4.0	High IP3, DBL-BAL, +4 LO	DC - 1.0	-8	32	25	LP4	EAR99	HMC215LP
1.8 - 2.2	High IP3, SGL-END	DC - 0.5	-8.5	25	31	MS8	EAR99	HMC402MS
2.0 - 2.7	High IP3, DBL-BAL, 0 LO	DC - 0.45	-7.5	25	31	LP4	EAR99	HMC688LP
2.0 - 2.7	High IP3, DBL-BAL, 0 LO	DC - 0.45	-7.5	26	31	LP4	EAR99	HMC689LP
2.3 - 4.0	High IP3, +4 LO	DC - 1	-10	15	35	LP4	EAR99	HMC615LP
2.4 - 4.0	High IP3, SGL-END	DC - 1	-10	30	34	MS8	EAR99	HMC214MS
3.1 - 3.9	High IP3, DBL-BAL, 0 LO	DC - 0.6	-8.5	28	30	LP4	EAR99	HMC666LP
6 - 12	High IP3, DBL-BAL	DC - 4	-8	40	30	LC3	EAR99	HMC663L0
9 - 15	High IP3, DBL-BAL	DC - 2.5	-7.5	40	24	MS8G	EAR99	HMC410AMS
ownconverte	r RF ICs							
0.7 - 3.5	High IP3 Dual Downconverter	0.05 - 0.35	7	55	+25	LP4	EAR99	HMC990LP
0.7 - 1.0	Downconverter	0.05 - 0.25	12.5	25	15	QS16	EAR99	HMC420QS
0.7 - 1.0	High IP3, Dual Downconverter	0.06 - 0.5	7.5	16	23	LP6C	EAR99	HMC683LP6
0.8 - 0.96	High IP3 Dual Downconverter	0.05 - 0.3	9	4	26	LP6	EAR99	HMC581LP
0.8 - 1.0	High IP3 Downconverter	0.05 - 0.25	13.8	28	15	QS16G	EAR99	HMC377QS1
0.8 - 2.7	Hi-IP3 Wideband Downconverter	0.001 - 0.6	-1	48	26	LP4	EAR99	HMC334LP
0.9 - 1.6	Hi-IP3 Downconverter with RF Amplifier	0.05 - 0.5	30	45	6	LP4	EAR99	HMC621LP
1.4 - 2.3	High IP3 Downconverter	0.05 - 0.3	9	33	19	QS16G	EAR99	HMC421QS
1.7 - 2.2	High IP3 Downconverter	0.05 - 0.3	11	25	19	QS16G	EAR99	HMC380QS1
1.7 - 2.2	High IP3, Dual Downconverter	50 - 300	9	10	27	LP6	EAR99	HMC381LP
1.7 - 2.2	High IP3, Dual Downconverter	0.06 - 0.4	6	25	25	LP6C	EAR99	HMC682LP6
1.8 - 2.7	High IP3 Downconverter with RF Amplifier	0.05 - 0.65	33	45	11	LP4	EAR99	HMC623LP
	Double & Single Balanced Mixers	2.00 0.00			•••			
0.6 - 1.3	Low LO, DBL-BAL	DC - 0.4	-8	35	15	MS8	EAR99	HMC423MS
0.0 - 1.3	0 LO, DBL-BAL	0.25 - 0.45	10	36	23	LP4	EAR99	HMC665LP
1.2 - 2.6	Low LO, DBL-BAL	DC - 1	-8	30	15	MS8	EAR99	HMC422MS
1.8 - 3.9	+3 LO, DBL-BAL	0.2 - 0.55	9	33	23	LP4	EAR99	HMC622LP
1.0 - 3.8	TO LO, DDL-DAL	0.2 - 0.00	9	JJ	23	Lr'4	LADSS	1 IIVIO022LP



### SMT & Chip (Die) Products

### **MIXERS**

RF Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	LO / RF Isolation (dB)	IIP3 (dBm)	Package	ECCN Code	Part Number
4 - 7	0 LO, DBL-BAL	DC - 2.5	-7	32	15	MS8G	EAR99	HMC488MS8G
4.5 - 6.0	+7 LO, DBL-BAL	DC - 1.6	-7	30	18	MS8	EAR99	HMC218MS8E
+10 dBm LO Doubl	e & Single Balanced Mixers							
0.7 - 2.0	+10 LO, DBL-BAL	DC - 0.3	-9	45	17	S8	EAR99	HMC207AMS8
0.7 - 2.0	+10 LO, DBL-BAL	DC - 0.5	-9	24	17	MS8	EAR99	HMC208AMS8
1.5 - 4.5	+10 LO, DBL-BAL	DC - 1.5	-8.5	40	19	MS8	EAR99	HMC213AMS8
1.7 - 3.0	+10 LO, SGL-BAL	DC - 0.8	-9	30	21	MS8	EAR99	HMC272AMS8
1.7 - 3.5	+10 LO, SGL-BAL	DC - 0.9	-9	30	21	SOT26	EAR99	HMC285E
4.5 - 8.0	+10 LO, DBL-BAL	DC - 2	-8.2	35	16	C8	EAR99	HMC168C8
5 - 12	+10 LO, DBL-BAL	DC - 4	-7.5	25	17	MS8	EAR99	HMC220AMS8
7 - 10	+10 LO, DBL-BAL	DC - 2	-9	32	16	C8	EAR99	HMC171C8
+13 to +14 dBm LO	Double & Triple Balanced M	ixers						
0.7 - 1.2	+13 LO, SGL-BAL	DC - 0.3	-9	26	21	MS8	EAR99	HMC277MS8
1.7 - 4.5	+13 LO, DBL-BAL	DC - 1	-8	30	20	MS8	EAR99	HMC175MS8I
1.7 - 4.5	+13 LO, Dual Channel	DC - 1.5	-8	-	23	LP5	EAR99	HMC340ALP5
2 - 18	Double Balance Mixer	DC - 2	-10	35	19	LC3B	EAR99	HMC1048LC3
2.5 - 4.0	+13 LO, DBL-BAL	DC - 2	-9	45	18	C8	EAR99	HMC170C8
4.5 - 9.0	+13 LO, DBL-BAL	DC - 2.5	-8.5	25	21	MS8	EAR99	HMC219AMS8
6 - 26	+13 LO, DBL-BAL	DC - 10	-9	32	20	Chip	EAR99	HMC773
6 - 26	+13 LO, DBL-BAL	DC - 8	-9	38	22	LC3B	EAR99	HMC773LC3
7 - 14	+13 LO, DBL-BAL	DC - 5	-7	48	22	Chip	EAR99	HMC553
7 - 14	+13 LO, DBL-BAL	DC - 5	-7	50	22	LC3B	EAR99	HMC553LC3
7 - 34	+13 LO, DBL-BAL	DC - 8	-11	35	22	LC3B	EAR99	HMC774LC3
7 - 43	+13 LO, DBL-BAL	DC - 10	-9	35	22	Chip	EAR99	HMC774
9 - 15	+13 LO, DBL-BAL	DC - 2.5	-7.5	40 - 50	17	MS8G	EAR99	HMC412AMS8
10 - 15	+13 LO, SGL-BAL	DC - 3	-9	27	16	MS8G	EAR99	HMC411MS80
11 - 20	+13 LO, DBL-BAL	DC - 6	-7	46	18	Chip	EAR99	HMC554
11 - 20	+13 LO, DBL-BAL	DC - 6	-7	46	18	LC3B	EAR99	HMC554LC3
14 - 26	+13 LO, DBL-BAL	DC - 8	-7.5	39	20	Chip	EAR99	HMC260
14 - 26	+13 LO, DBL-BAL	DC - 8	-7.5	38	20	LC3B	EAR99	HMC260LC3
16 - 30	+13 LO, DBL-BAL	DC - 8	-8	40	21	LC3B	EAR99	HMC292LC3
17 - 31	+13 LO, DBL-BAL	DC - 6	-8	32	19	LM3C	EAR99	HMC292LM3
18 - 32	+13 LO, DBL-BAL	DC - 8	-7.5	38	19	Chip	EAR99	HMC292
24 - 32	+13 LO, DBL-BAL	DC - 8	-10	38	19	LC3B	EAR99	HMC329LC3
24 - 40	+13 LO, DBL-BAL	DC - 18	-8	35	21	Chip	EAR99	HMC560
24 - 40	+13 LO, DBL-BAL	DC - 17	-10	35	21	LM3	EAR99	HMC560LM
25 - 40	+13 LO, DBL-BAL	DC - 8	-9.5	42	19	Chip	EAR99	HMC329
26 - 32	+13 LO, TPL-BAL	16 - 22	-10	45	22	Chip	EAR99	HMC1015
26 - 32	+13 LO, TPL-BAL	16 - 22	-10	45	23	LC3	EAR99	HMC1043LC
26 - 40	+13 LO, DBL-BAL	DC - 8	-8	37	19	LM3	EAR99	HMC329LM3
54 - 64	+13 LO, DBL-BAL	DC - 5	-8	30	13	Chip	5A991.h	HMC-MDB16
70 - 90	+14 LO, DBL-BAL	DC - 18	-12	-	-	Chip	5A991.h	HMC-MDB27
	Single, & Double Balanced					01:	F. F. F. F.	,,,,,,,,
1.8 - 5.0	+15 LO, DBL-BAL	DC - 3	-7	42	18	Chip	EAR99	HMC128
1.8 - 5.0	+15 LO, DBL-BAL	DC - 2	-10	40	18	G8 Hermetic	EAR99	HMC128G8
2.5 - 7	+15 LO, DBL-BAL	DC - 3	-7	48	22	Chip	EAR99	HMC557
2.5 - 7	+15 LO, DBL-BAL	DC - 3	-7	48	22	LC4	EAR99	HMC557LC4
4 - 8	+15 LO, DBL-BAL	DC - 3	-7	40	17	Chip	EAR99	HMC129
4 - 8	+15 LO, DBL-BAL	DC - 3	-8	30	18	G8 Hermetic	EAR99	HMC129G8
4 - 8	+15 LO, DBL-BAL	DC - 3	-7	40	17	LC4	EAR99	HMC129LC4
5.5 - 14	+15 LO, DBL-BAL	DC - 6	-7	45	24	Chip	EAR99	HMC558
5.5 - 14	+15 LO, DBL-BAL	DC - 6	-7	45	24	LC3B Chin	EAR99	HMC558LC3
6 - 11	+15 LO, DBL-BAL	DC - 2	-7	40	17	Chip	EAR99	HMC141C8 / 14
6 - 15	+15 LO, DBL-BAL	DC - 2	-8.5	35	20	C8	EAR99	HMC141C8 / 14
6 - 18	+15 LO, DBL-BAL	DC - 6	-10	25	21	Chip	EAR99	HMC141 / 14
7 - 14	+15 LO, DBL-BAL	DC - 2	-10	35	20	LH5 Hermetic	EAR99	HMC141LH5
14 - 23	+15 LO, DBL-BAL	DC - 2	-10.5 -9	38	18	Chip	EAR99	HMC203
3 - 10	+17 LO, DBL-BAL	DC - 4		55	23	LC3B Chin	EAR99	HMC142 / 14
5 - 20 6 - 20	+20 LO, DBL-BAL +20 LO, DBL-BAL	DC - 3	-10 -10	30 35	25 23	Chip LC4	EAR99 EAR99	HMC143 / 14 HMC144LC4
	+/U I U DBI-BAI	130 3	- (()	.15		11.4	FARSS	mivi(, 1441 (; 2



### **SMT & Chip (Die) Products**

### **MIXERS**

RF Frequency (GHz)			Conversion Gain (dB)	LO / RF Isolation (dB)	IIP3 (dBm)	Package	ECCN Code	Part Number
Sub-Harmonic M	ixers							
14 - 20	Sub-Harmonic	DC - 3	-10	40	7	LM3	EAR99	HMC258LM3
14 - 21	Sub-Harmonic	DC - 3	-10	40	7	Chip	EAR99	HMC258
14.5 - 19.5	Sub-Harmonic	DC - 3.5	-10	45	5	LC3B	EAR99	HMC258LC3B
17 - 25	Sub-Harmonic	DC - 3	-9	27	10	Chip	EAR99	HMC337
17.7 - 23.6	Sub-Harmonic, Upconverter	DC - 3.5	15	40	13	LC5	EAR99	HMC711LC5
20 - 30	Sub-Harmonic	DC - 4	-9	30	10	LM3	EAR99	HMC264LM3
20 - 31	Sub-Harmonic, Downconverter	0.7 - 3.0	3	28	8	LM3	EAR99	HMC265LM3
20 - 32	Sub-Harmonic	DC - 6	-10	40	13	Chip	EAR99	HMC264
20 - 32	Sub-Harmonic, Downconverter	0.7 - 3.0	3	30	10	Chip	EAR99	HMC265
20 - 40	Sub-Harmonic	1 - 3	-12	24	13	Chip	EAR99	HMC266
21 - 31	Sub-Harmonic	DC - 6	-9	40	13	LC3B	EAR99	HMC264LC3B
24 - 34	Sub-Harmonic	DC - 3	-11	33	13	LC3B	5A991.b	HMC338LC3B
24 - 34	Sub-Harmonic	DC - 4	-10	30	22	LC4	EAR99	HMC798LC4
26 - 33	26 - 33 Sub-Harmonic		-9	33	11	Chip	5A991.b	HMC338
33 - 42	Sub-Harmonic	DC - 3	-10	37	10	Chip	EAR99	HMC339

### **DEMODULATORS - I/Q Demodulator**

Input Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	Noise Figure (dB)	IIP3 / IIP2 (dBm)	Package	ECCN Code	Part Number
0.1 - 4.0	I/Q Demodulator	DC - 0.6	-3.5	15	+25 / +60	LP4	EAR99	HMC597LP4E

### **MODULATORS - Bi-Phase Modulator**

Input Frequency (GHz)	Function	Loss (dB)	Amp / Phase Balance (dB/Deg)	Carrier Suppression (dBc)	Bias Control (mA)	Package	ECCN Code	Part Number
1.8 - 5.2	Bi-Phase	8	0.2 / 2.5	30	+/-5	Chip	EAR99	HMC135
4 - 8	Bi-Phase	8	0.1 / 4.0	30	+/-5	Chip	EAR99	HMC136
6 - 11	Bi-Phase	9	0.25 / 10.0	20	+/-5	Chip	EAR99	HMC137

### **MODULATORS - Direct Quadrature Modulator**

Input Freq. (GHz)	Function	OIP3 (dBm) / Carrier Suppression (dBc)	Modulation Bandwidth (MHz)	Output Noise Floor (dBc/Hz)	Bias Supply	Package	ECCN Code	Part Number
0.02 - 2.7	Direct Quadrature	23 / 42	DC - 700	-162	+5V @ 160 mA	LP4	EAR99	HMC696LP4E
0.05 - 2.8	Direct Quadrature with VGA	25 / 50	DC - 440	-159	+5V @ 120 mA	LP5	3A001.a.11.b	HMC795LP5E
0.1 - 4.0	Direct Quadrature	23 / 42	DC - 700	-159	+5V @ 170 mA	LP4	EAR99	HMC497LP4E
0.1 - 6.0	Direct Quadrature	30 / 40	DC - 700	-160	+5V @170 mA	LP4	EAR99	HMC1097LP4E
0.25 - 3.8	Direct Quadrature	14 / 38	DC - 250	-158	+3.3V @ 108 mA	LP3	EAR99	HMC495LP3E
0.45 - 4.0	Direct Quadrature	22 / 43	DC - 700	-165	+5V @ 168 mA	LP4	EAR99	HMC697LP4E
4 - 7	Direct Quadrature	17 / 34	DC - 250	-157	+3V @ 93 mA	LP3	EAR99	HMC496LP3E

### **MODULATORS - Vector Modulators**

Frequency (GHz)	Function	Gain Range (dB)	Continuous Phase Control (deg)	IP3 / Noise Floor (Ratio)	IIP3 @ Max. Gain (dBm)	Package	ECCN Code	Part Number
0.7 - 1.0	Vector	-50 to -10	360	186.5	34	LP3	EAR99	HMC630LP3E
1.8 - 2.7	Vector	-50 to -10	360	186	35	LP3	EAR99	HMC631LP3E
1.8 - 2.2	Vector	-50 to -10	360	185	33	LP3	EAR99	HMC500LP3E

### PASSIVES - Fixed Attenuators

Frequency (GHz)	Function	Attenuation Accuracy (dB)	Nominal Attenuation (dB)	Maximum Input Power (dBm)	Chip Size (Mils)	Package	ECCN Code	Part Number
DC - 50	Thru Line	±0.2	0.15	-	17 x 18	Chip	EAR99	HMC650
DC - 50	Thru Line	±0.3	0.15	-	23 x 18	Chip	EAR99	HMC651
DC - 50	Passive	±0.2	2	27	17 x 18	Chip	EAR99	HMC652
DC - 25	Passive	±0.5	2	27	-	LP2	EAR99	HMC652LP2E
DC - 50	Passive	±0.2	3	26	17 x 18	Chip	EAR99	HMC653
DC - 25	Passive	±0.5	3	26	-	LP2	EAR99	HMC653LP2E
DC - 50	Passive	±0.2	4	25	17 x 18	Chip	EAR99	HMC654
DC - 25	Passive	±0.5	4	25	-	LP2	EAR99	HMC654LP2E
DC - 50	Passive	±0.2	6	26	17 x 18	Chip	EAR99	HMC655
DC - 25	Passive	±0.5	6	26	-	LP2	EAR99	HMC655LP2E
DC - 50	Passive	±0.1	10	25	17 x 18	Chip	EAR99	HMC656
DC - 25	Passive	±1.5	10	25	N/A	LP2	EAR99	HMC656LP2E
DC - 50	Passive	±0.4	15	25	17 x 18	Chip	EAR99	HMC657



### SMT & Chip (Die) Products

### **PASSIVES - Fixed Attenuators**

Frequency (GHz)	Function	Attenuation Accuracy (dB)	Nominal Attenuation (dB)	Maximum Input Power (dBm)	Chip Size (Mils)	Package	ECCN Code	Part Number
DC - 25	Passive	±2	15	25	N/A	LP2	EAR99	HMC657LP2E
DC - 50	Passive	±0.5	20	25	23 x 18	Chip	EAR99	HMC658
DC - 25	Passive	±2	20	25	N/A	LP2	EAR99	HMC658LP2E

PHASE SHIFTERS - Analog

TIAGE SITI	I ILIIO - Alla	iiog						
Frequency (GHz)	Function	Insertion Loss (dB)	Phase Range (deg)	2nd Harmonic Pin = -10 dBm (dBc)	Control Voltage Range (Vdc)	Package	ECCN Code	Part Number
1 - 2	Analog	3.5	400°	-40	0 to +13V	LP5	EAR99	HMC934LP5E
2 - 4	Analog	3.5	480° @ 2 GHz 450° @ 4 GHz	-40	0V to +13V	LP5	EAR99	HMC928LP5E
2 - 20	Analog	4	270° @ 2 GHz 180° @ 20 GHz	-45	0.5 to +11V	LP5	EAR99	HMC935LP5E
4 - 8	Analog	4	450° @ 4 GHz 430° @ 8 GHz	-40	0V to +13V	LP4	EAR99	HMC929LP4E
5 - 18	Analog	4	500° @ 5 GHz 100° @ 18 GHz	-80	0V to +10V	Chip	EAR99	HMC247
6 - 15	Analog	7	750° @ 6 GHz 500° @ 15 GHz	-40	0V to +5V	LP4	EAR99	HMC538LP4E
8 - 12	Analog	3.5	425° @ 8 GHz 405° @ 12 GHz	-35	0 to +13V	LP4	EAR99	HMC931LP4E
8 - 23	Analog	-	500°	-35	2.7 to 3.9V	LC3	3A001.a.11.b	HMC877LC3
12 - 18	Analog	4	405° @ 12 GHz 385° @ 18 GHz	-40	0 to +13V	LP4	EAR99	HMC932LP4E
18 - 24	Analog	4.5	495° @ 18 GHz 460° @ 24 GHz	-37	0 to +13V	LP4	EAR99	HMC933LP4E

### **PHASE SHIFTERS - Digital**

Frequency (GHz)	Function	Insertion Loss (dB)	Phase Range (deg)	IIP3 (dBm)	Control Input (Vdc)	Package	ECCN Code	Part Number
8 - 12	-Bit Digital	5	22.5 to 360	40	0 / -3V	Chip	EAR99	HMC543
8 - 12	4-Bit Digital	6.5	22.5 to 360	37	0 / -3V	LC4B	EAR99	HMC543LC4B
15 - 18.5	5-Bit Digital	7	11.25 to 360	40	0 / -3	Chip	EAR99	HMC644
15 - 18.5	5-Bit Digital	7	11.25 to 360	40	0 / -3	LC5	EAR99	HMC644LC5
1.2 - 1.4	6-Bit Digital	4	5.625 to 360	45	0 / +5V	LP6	EAR99	HMC936LP6E
2.5 - 3.1	6-Bit Digital	4	5.625 to 360	54	0 / +5	Chip	EAR99	HMC647
2.5 - 3.1	6-Bit Digital	4	5.625 to 360	54	0 / +5	LP6	EAR99	HMC647LP6E
2.9 - 3.9	6-Bit Digital	4	5.625 to 360	45	0 / +5	Chip	EAR99	HMC648
2.9 - 3.9	6-Bit Digital	5	5.625 to 360	45	0 / +5	LP6	EAR99	HMC648LP6E
3 - 6	6-Bit Digital	6.5	5.625 to 360	44	0 / +5	Chip	EAR99	HMC649
3 - 6	6-Bit Digital	8	5.625 to 360	44	0 / +5	LP6	EAR99	HMC649LP6E
9 - 12	6-Bit Digital	6.5	5.625 to 360	38	0 / -3	Chip	EAR99	HMC643
9 - 12	6-Bit Digital	7	5.625 to 360	38	0 / -3	LC5	EAR99	HMC643LC5
9 - 12.5	6-Bit Digital	6.5	5.625 to 360	41	0 / +5	Chip	EAR99	HMC642
9 - 12.5	6-Bit Digital	7	5.625 to 360	41	0 / +5	LC5	EAR99	HMC642LC5

POWER DETECTORS - Log Detector/Controllers & RMS Detectors

Frequency (GHz)	Function	Dynamic Range (dB)	RSSI Slope (mV/dB)	RF Threshold Level (dBm)	Bias Supply	Package	ECCN Code	Part Number
50 Hz - 3.0	Log Detector / Controller	74 ±3	19	-66	+3.3V @ 29 mA	LP4	EAR99	HMC612LP4E
0.001 - 8.0	Log Detector / Controller	70 ±3	-25	-61	+5V @ 113 mA	LP4	EAR99	HMC602LP4E
0.001 - 10.0	Log Detector / Controller	73 ±3	-25	-65	+5V @ 103 mA	Chip	EAR99	HMC611
0.001 - 10.0	Log Detector / Controller	70 ±3	-25	-65	+5V @ 106 mA	LP4	EAR99	HMC611LP4E
0.01 - 4.0	Log Detector / Controller	70 ±3	19	-68	+3.3V @ 30 mA	LP4	EAR99	HMC601LP4E
0.05 - 4.0	Log Detector / Controller	70 ±3	19	-69	+3.3V @ 29 mA	LP4	EAR99	HMC600LP4
0.05 - 8.0	Log Detector / Controller	54 ±1	17.5	-55	+5V @ 17 mA	LP3	EAR99	HMC713LP3
0.1 - 2.7	Log Detector / Controller	54 ±1	17.5	-52	+5V @ 17 mA	MS8	EAR99	HMC713MS8
8 - 30	Log Detector	54 ±3	13.3	-55	+3.3V @ 88 mA	LP3	EAR99	HMC662LP3
1 - 23	mmW Power Detector	56 ±3	14.2	-52	+3.3V @ 91 mA	LP3	3A001.b.2.c	HMC948LP3
DC - 3.9	RMS Power Detector	60 ±1	37	-69	+5V @ 50 mA	LP4	EAR99	HMC1010LP4
DC - 3.9	RMS, Single-Ended	72 ±1	35	-68	+5V @ 55 mA	LP4	EAR99	HMC1020LP4
DC - 3.9	RMS, Single-Ended with Envelope Tracker	70 ±1	35	-68	+5V @ 75 mA	LP4	EAR99	HMC1021LP4
DC - 3.9	Dual RMS, Single-Ended	70 ±1	38.5	-66	+5V @ 143 mA	LP5	EAR99	HMC1030LP5
DC - 5.8	RMS Power Detector	40 ±1	37	-69	+5V @ 42 mA	LP4	EAR99	HMC909LP4



### **SMT & Chip (Die) Products**

**SDLVAs - Successive Detection Log Video Amplifiers** 

Frequency (GHz)	Function	Dynamic Range (dB)	RSSI Slope (mV/dB)	RF Threshold Level (dBm)	Bias Supply	Package	ECCN Code	Part Number
0.1 - 20	SDLVA	59	14	-54	+3.3V @ 83 mA	LC4B	EAR99	HMC613LC4B
0.5 - 18.5	SDLVA, Extended Range	67	15	-62	+3.3V @ 183 mA	LP4	EAR99	HMC1013LP4E
0.6 - 20	SDLVA	59	14	-54	+3.3V @ 80 mA	Chip	EAR99	HMC913
0.6 - 20	SDLVA	59	14	-54	+3.3V @ 80 mA	LC4B	EAR99	HMC913LC4B
1 - 20	SDLVA with Limited RF Output	55	15	-53	+3.3V @ 153 mA	LC4B	EAR99	HMC813LC4B
1 - 26	SDLVA with Limited RF Output	55	14.5	-53	+3.3V @ 150 mA	Chip	EAR99	HMC813

#### SWITCHES

<b>SWITCHES</b>								
Frequency (GHz)	Function	Insertion Loss (dB)	Isolation (dB)	Input P1dB (dBm)	Control Input (Vdc)	Package	ECCN Code	Part Number
SPST & SPDT S	Switches							
DC - 6	SPST, Failsafe	0.7	25	27	0 / +2.2 to +5V	SOT26	EAR99	HMC550E
DC - 6	SPST, High Isolation	1.4	52	27	0 / -5V	G7 Hermetic	EAR99	HMC231G7
DC - 2.5	SPDT, Reflective	0.4	36	29	0 / -5V	S8	EAR99	HMC239AS8E
DC - 3	SPDT, Reflective	0.4	27	30	0 / +3V	MS8	EAR99	HMC190AMS8E
DC - 3	SPDT, High Isolation	0.7	50	23	0 / +5V	MS8	EAR99	HMC194MS8E
DC - 3	SPDT, Reflective	0.4	28	30	0 / +3V	SOT26	EAR99	HMC197AE
DC - 3	SPDT, Reflective	0.4	28	30	0 / +3V	SOT26	EAR99	HMC221AE
DC - 3	SPDT, Reflective	0.3	31	34	0 / +3 to +8V	SOT26	EAR99	HMC545E
DC - 3.5	SPDT, High Isolation	0.5	45	25	0 / +5V	MS8G	EAR99	HMC284MS8GE
DC - 4	SPDT, Reflective	0.5	28	29	0 / -5V or +5V / 0	Chip	EAR99	HMC240A
DC - 4	SPDT, High Isolation	0.9	65	31	0 / +5V	LP4C	EAR99	HMC349LP4CE
DC - 4	SPDT, High Isolation	0.9	57	31	0 / +5V	MS8G	EAR99	HMC349MS8GE
DC - 4	SPDT, High Isolation	1.1	47	31	0 / +5V	MS8G	EAR99	HMC435MS8GE
DC - 4	SPDT, Differential	0.8	45	35	0 / +3V to	LP4	EAR99	HMC922LP4E
DC - 6	SPDT, High Isolation	1.4	50	26	0 / -5V	G7 Hermetic	EAR99	HMC232G7
DC - 6	SPDT, High Isolation	1.4	43	26	0 / -5V	G8 Hermetic	EAR99	HMC232G8
DC - 6	SPDT, High Isolation	1.4	43	26	0 / -5V	G8 Hermetic	EAR99	HMC233G8
DC - 6	SPDT, High Isolation	1.6	42	25	0 / +5V	MS8G	EAR99	HMC336MS8GE
DC - 6	SPDT, High Isolation	1.4	46	27	0 / -5V	G7 Hermetic	EAR99	HMC607G7
DC - 6	SPDT, High Isolation	0.8	60	35	0 / +3 to +5V	LP4C	EAR99	HMC849LP4CE
DC - 8	SPDT, High Isolation	1.4	50	26	0 / -5V	C8	EAR99	HMC232C8
DC - 8	SPDT, High Isolation	1.5	45	26	0 / -5V	C8	EAR99	HMC234C8
DC - 8	SPDT, High Isolation	1.2	48	23	0 / -5V	MS8G	EAR99	HMC270MS8GE
DC - 8	SPDT, High Isolation	2.0	44	23	0 / -5V	C8	EAR99	HMC347C8
DC - 8	SPDT, High Isolation	2.2	35	23	0 / -5V	G8 Hermetic	EAR99	HMC347G8
DC - 12	SPDT, High Isolation	1.5	55	27	0 / -5V	LP4	EAR99	HMC232LP4E
DC - 14	SPDT, High Isolation	1.7	44	23	0 / -5V	LP3	EAR99	HMC347LP3E
DC - 14	SPDT, High Isolation	1.4	50	26	0 / -5V	Chip	EAR99	HMC232
DC - 15	, ,	1.7	60	26	0 / -5V	<u> </u>	EAR99	
	SPDT, High Isolation	1.7				Chip		HMC607
DC - 20	SPDT, High Isolation		45	23	0 / -5V	Chip	EAR99	HMC347
DC - 20	SPDT, High Isolation	1.8	47	23	0 / -5V	LP3	EAR99	HMC547LP3E
DC - 28	SPDT, High Isolation	1.8	47	23	0 / -5V	LC3	EAR99	HMC547LC3
0.1 - 50	SPDT, Reflective	1.9	31	25	0 / -3V	Chip	EAR99	HMC986
55 - 86	SPDT, PIN MMIC		30	-	-5 / +5	Chip	5A991.h	HMC-SDD112
0.1 - 2.1	SPDT, 40W, Failsafe	0.4	22	46	0 / +3V to +8V	LP2	EAR99	HMC646LP2E
0.2 - 2.2	SPDT, 10W, Failsafe	0.4	40	> 40	0 / +3 to +8V	MS8G	EAR99	HMC546MS8GE
0.2 - 2.7	SPDT, 10W, Failsafe	0.4	35	43	0 / +3 to +8V	LP2	EAR99	HMC546LP2E
0.824 - 0.894	SPDT, 10W, T/R	0.6	22	> 40	0 / +5V	SOT26	EAR99	HMC446E
DC - 2.5	SPDT, CATV	0.6	58	28	0 / +5V	LP3	EAR99	HMC348LP3E
DC - 3	SPDT T/R	0.5	25	39	0/ +3V to +8V	MS8	EAR99	HMC174MS8E
DC - 3	SPDT, 5W, T/R	0.3	30	39	0 / +3 to +10V	MS8	EAR99	HMC574MS8E
DC - 3	SPDT, 3W, T/R	0.3	30	37	0 / +3 to +10V	SOT26	EAR99	HMC595E
DC - 4	SPDT T/R	0.25	23	39	0 / +3 to +5V	SOT26	EAR99	HMC544E
DC - 4	SPDT, 10W, T/R	0.4	30	40	0 / +3 to +8V	MS8G	EAR99	HMC784MS8GE
DC - 6	SPDT T/R	0.5	27	37	0 / +3 to +5V	MS8G	EAR99	HMC536MS8GE
DC - 6	SPDT T/R	0.6	27	37	0 / +3 to +5V	LP2	EAR99	HMC536LP2E
5 - 6	SPDT T/R	1.2	31	33	TTL/CMOS	MS8	EAR99	HMC224MS8E



### SMT & Chip (Die) Products

### **SWITCHES**

Frequency (GHz)	Function	Insertion Loss (dB)	Isolation (dB)	Input P1dB (dBm)	Control Input (Vdc)	Package	ECCN Code	Part Number
Multi-Throw Sw	itches							
DC - 3.5	SP3T	0.5	44	26	TTL/CMOS	QS16	EAR99	HMC245QS16E
DC - 2	SP4T	0.8	32	24	0 / -5V	S14	EAR99	HMC182S14E
DC - 3.5	SP4T	0.5	45	25	TTL/CMOS	QS16	EAR99	HMC241QS16E
DC - 4	SP4T	0.6	47	26	TTL/CMOS	LP3	EAR99	HMC241LP3E
DC - 4	SP4T	0.7	40	25	TTL/CMOS	G16 Hermetic	EAR99	HMC244G16
DC - 8	SP4T	1.8	42	21	0 / -5V	Chip	EAR99	HMC344
DC - 8	SP4T	2.0	45	26	0 / -5V	LC3	EAR99	HMC344LC3
DC - 8	SP4T	1.8	40	21	0 / -5V	LP3	EAR99	HMC344LP3E
DC - 8	SP4T	2.2	32	21	0 / 5V	LP3	EAR99	HMC345LP3E
DC - 12	SP4T	1.8	42	27	0 / -5V	LH5 Hermetic	EAR99	HMC344LH5
DC - 18	SP4T	2.1	42	24	0 / -5V	Chip	EAR99	HMC641
DC - 20	SP4T	2.1	42	23	0 / -5V	LC4	EAR99	HMC641LC4
DC - 20	SP4T	2.3	45	22	0 / -5V	LP4	EAR99	HMC641LP4E
23 - 30	SP4T	2.8	35	25	0 / -3V	LC4	EAR99	HMC944LC4
DC - 3	SP6T	0.8	41	24	TTL/CMOS	QS24	EAR99	HMC252QS24E
DC - 2	SP8T	1.3	30	20	0 / -5V	QS24	EAR99	HMC183QS24E
DC - 2.5	SP8T	1.1	36	23	TTL/CMOS	QS24	EAR99	HMC253QS24E
DC - 3.5	SP8T	1.2	36	24	TTL/CMOS	LC4	EAR99	HMC253LC4
DC - 8	SP8T	2.3	40	23	0 / 5V	LP4	EAR99	HMC321LP4E
DC - 8	SP8T	2.5	25	23	0 / -5V	LP4	EAR99	HMC322LP4E
DC - 10	SP8T	2	38	23	0 / -5V	Chip	EAR99	HMC322
Bypass, Diversi	ty, Matrix & Transfer S	witches						
DC - 2.5	Bypass DPDT	0.3	25	23	0 / +5V	MS8	EAR99	HMC199MS8E
5 - 6	DPDT, Diversity	1.2	20	30	0 / +5V	MS8G	EAR99	HMC393MS8GE
0.2 - 3.0	4x2 Matrix	6	44	26	0 / +5V	LP4	EAR99	HMC276LP4E
0.2 - 3.0	4x2 Matrix	6.5	43	22	0 / +3 to +5V	LP4	EAR99	HMC596LP4E
0.7 - 3.0	4x2 Matrix	5.8	33	26	0 / +5V	QS24	EAR99	HMC276QS24E
DC - 8	Transfer	1.2	42	26	0 / +5V	LP3	EAR99	HMC427LP3E

### TRANSCEIVERS - New Product Line!

	Frequency (GHz)	Function	P1dB (dBm) NF (dB)	Max Gain (dB)	Gain Adjust (dB)	Phase Noise @ 1 MHz Offset (dBc/Hz)	Power Dissipation (W)	Package	ECCN Code	Part Number
NEW!	57 - 64	60 GHz Integrated Transmitter	12 dBm	38	17	-86	0.8	Chip	5A991.b	HMC6000
NEW!	57 - 64	60 GHz Integrated Receiver	6 dB	67	65	-86	0.61	Chip	5A991.b	HMC6001

### **VARIABLE GAIN AMPLIFIERS**

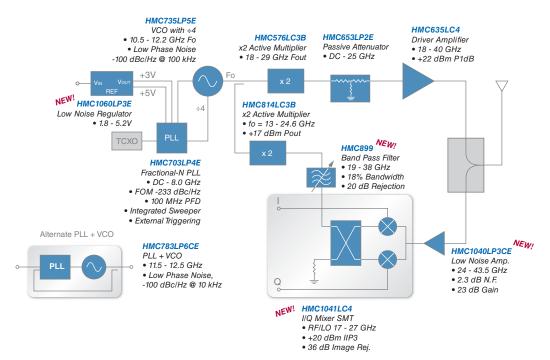
Frequency (GHz)	Function	Gain Control Range (dB)	NF * (dB)	OIP3 * (dBm)	P1dB (dBm)	Bias Supply	Package	ECCN Code	Part Number
0.5 - 6.0	Analog	-35 to 15	7.5	28	21	+5V @ 90 mA	LP5	EAR99	HMC972LP5E
2.3 - 2.5	Analog	-8 to 22	2.5	7	3	+3V @ 9 mA	MS8	EAR99	HMC287MS8E
5 - 12	Analog	22	2	34	23	+5V @ 120 mA	LP4	EAR99	HMC996LP4E
6 - 17	Analog	0 to 23	5	30	22	+5V @ 170 mA	Chip	EAR99	HMC694
6 - 17	Analog	0 to 23	6	30	22	+5V @ 175 mA	LP4	EAR99	HMC694LP4E
17 - 27	Analog	15	3.5	30	24	+5V @ 170 mA	LC4	EAR99	HMC997LC4
0.03 - 0.4	5-Bit digital, Differential Outputs	-4 to 19	5	40	25	+5V @ 240 mA	LP4	EAR99	HMC680LP4E
0.05 - 0.8	5-Bit Digital	-8 to 15	5	35	18	+5V @ 65 mA	LP4	EAR99	HMC628LP4E
0.07 - 4.0	6-Bit Digital, Serial & Parallel Control	-19.5 to 12	4	39	23	+5V @ 150 mA	LP5	EAR99	HMC742LP5E
0.5 - 4.0	6-Bit Digital, Serial & Parallel Control or Latched Parallel Control	-19 to 12.5	4	39	21.5	+5V @ 150 mA	LP5	EAR99	HMC742HFLP5E
0.7 - 1.2	6-Bit Digital, Serial & Parallel Control	-2.5 to 29	0.8	38.5	21	+5V @ 236 mA	LP5	EAR99	HMC707LP5E
0.7 - 2.7	6-Bit Digital	6.5 to 38	4.4	45	25	+5V @ 218 mA	LP5	EAR99	HMC926LP5E
DC - 1	6-Bit Digital, Serial & Parallel Control	-11.5 to 20	4.3	36	20	+5V @ 90 mA	LP5	EAR99	HMC627LP5E
DC - 1	6-Bit Digital, Parallel Control	8.5 to 40	2.8	36	20	+5V @ 176 mA	LP5	EAR99	HMC626LP5E
DC - 1	6-Bit Digital, Serial Control	13.5 to 45	2.7	36	20	+5V @ 176 mA	LP5	EAR99	HMC681LP5E
DC - 6	6-Bit Digital, Serial & Parallel Control	-13.5 to 18	6	33	19	+5V @ 88 mA	LP5	EAR99	HMC625LP5E
0.5 - 6.0	6-Bit Digital, Serial & Parallel Control	-13.5 to 18	6	33	19	+5V @ 88 mA	LP5	EAR99	HMC625HFLP5E
1.7 - 2.2	6-Bit Digital, Serial & Parallel Control	-2.5 to 29	1.0	37.5	21.5	+5V @ 252 mA	LP5	EAR99	HMC708LP5E
DC - 4	Dual 6-Bit Digital, Serial Control	-45 to 18	6	33	18	+5V @ 82 mA	LP6C	EAR99	HMC743LP6CE

<sup>\*</sup> Maximum Gain State



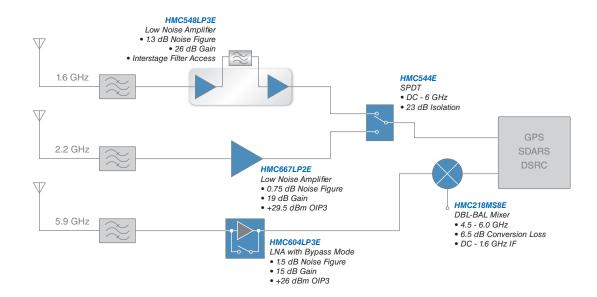
### Automotive: Telematics & Sensors, 2 - 110 GHz

#### 24 GHz FMCW AUTOMOTIVE SENSOR



Typical Automotive application is illustrated. See the full product listing for alternatives to the HMC products shown in each functional block.

### GPS, SDARS & DSRC RF FRONT-END FOR TELEMATICS



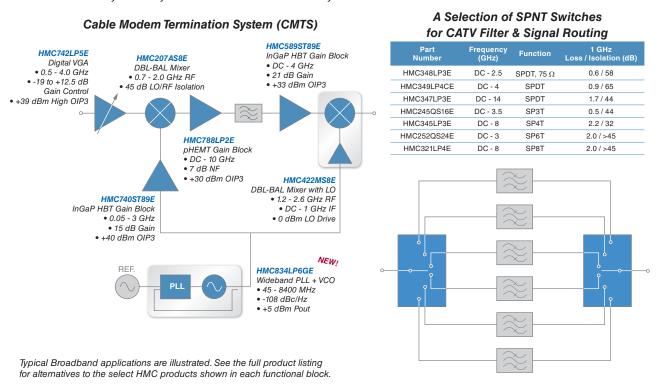
Typical Automotive application is illustrated.

See the full product listing for alternatives to the select HMC products shown in each functional block.

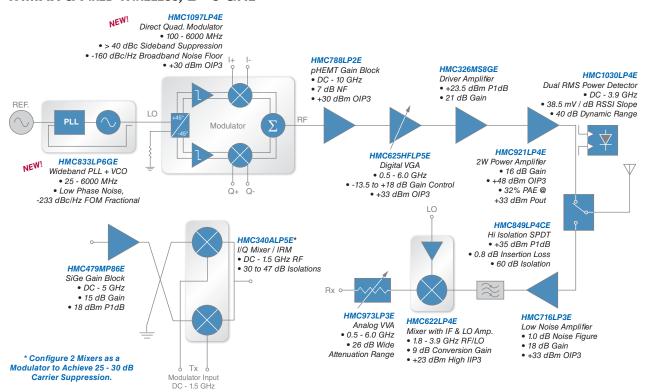


### Broadband, DC - 11 GHz

### CABLE MODEM, CATV, DBS & VoIP Solutions, 5 - 2150 MHz



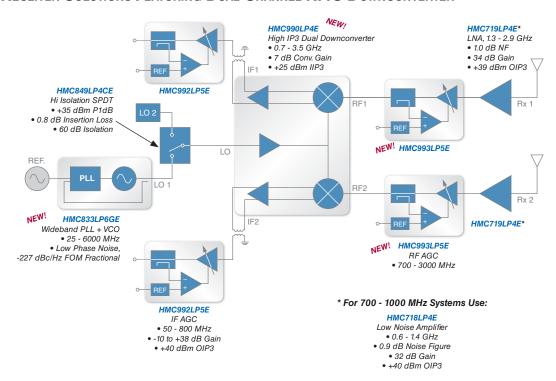
### WIMAX & FIXED WIRELESS, 2 - 6 GHz



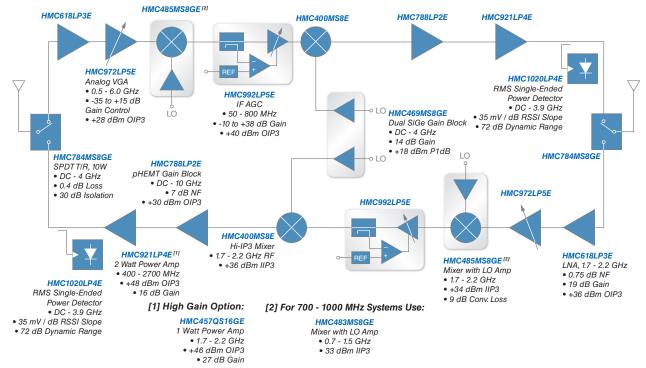


### Cellular Infrastructure, 380 - 2690 MHz

### BTS Receiver Solutions Featuring Dual Channel RFIC Downconverter



### CDMA/GSM/TD-SCDMA REPEATER SOLUTIONS

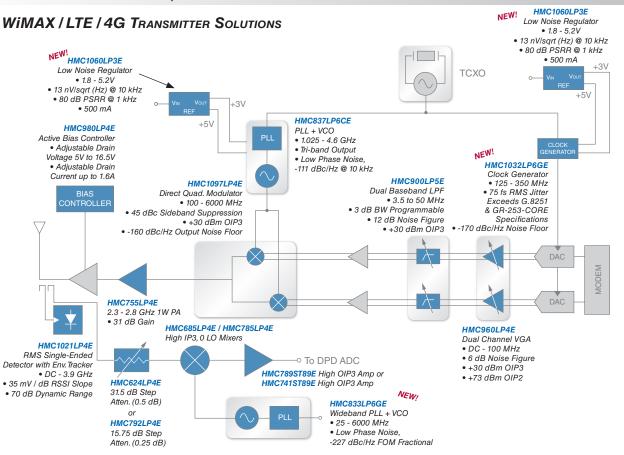


Typical Cellular/PCS/3G applications are illustrated.

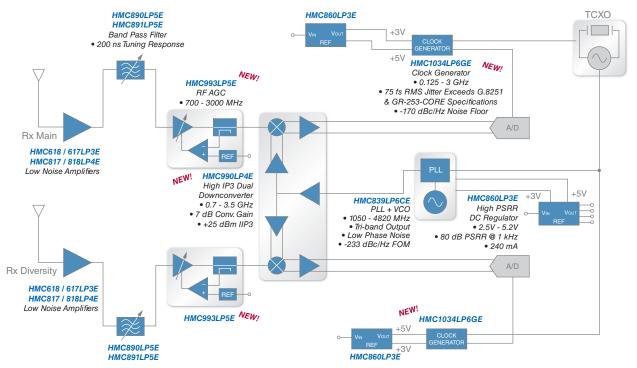
See the full product listing for alternatives to the select HMC products shown in each functional block.



### Cellular Infrastructure, 380 - 2690 MHz



### WIMAX / LTE / 4G RECEIVER SOLUTIONS FEATURING HETERODYNE DOWNCONVERSION

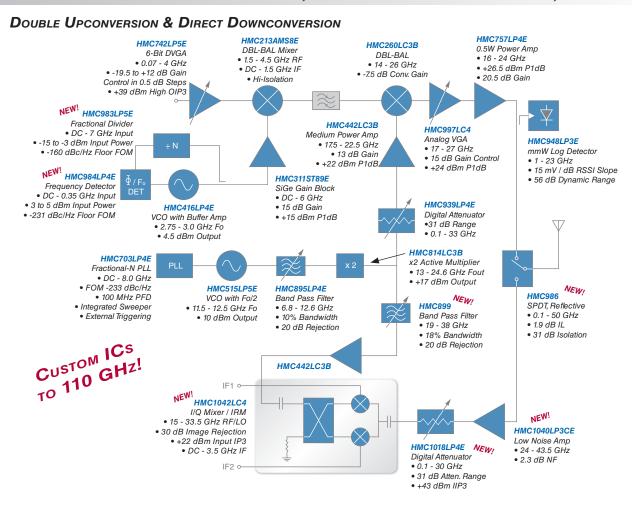


Typical WiMAX/LTE/4G applications are illustrated.

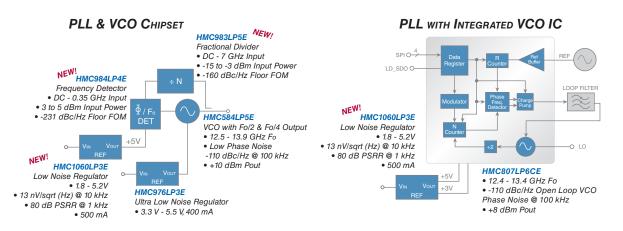
See the full product listing for alternatives to the select HMC products shown in each functional block.



### Microwave & mmWave Communications, Test & Measurement & Sensors, 2 - 86 GHz



### HITTITE'S HIGH FREQUENCY LO SOURCE ALTERNATIVES



Typical Microwave / Millimeterwave application is illustrated.

See the full product listing for alternatives to the select HMC products shown in each functional block.

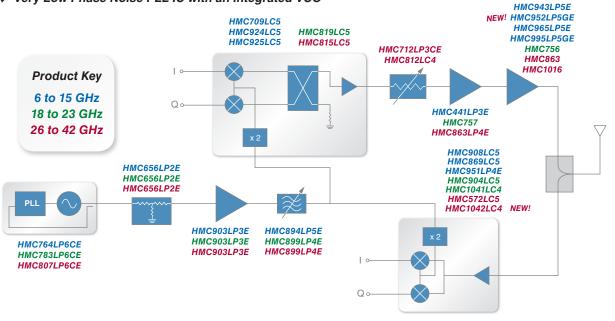


### Microwave & mmWave Communications, Test & Measurement & Sensors, 2 - 86 GHz

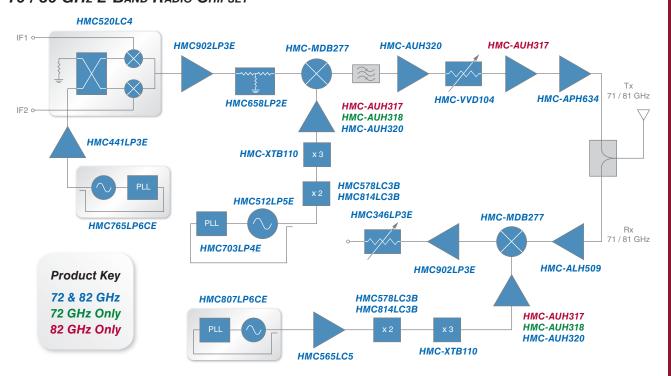
### CHIPSETS FOR 6 TO 42 GHZ MICROWAVE RADIO BACKHAUL

#### **Features**

- ♦ Integrated IQ TX Upconverter IC with a X2 LO Buffer & a High Linearity Driver Amplifier
- ♦ High Linearity 17 24 GHz Power Amplifier with 40 dBm OIP3 & 32 dBm Saturated Power
- ♦ Low Noise Image Rejection Downconverter IC with a X2 Integrated LO Buffer
- ♦ Very Low Phase Noise PLL IC with an Integrated VCO



### 70 / 80 GHz E-BAND RADIO CHIPSET





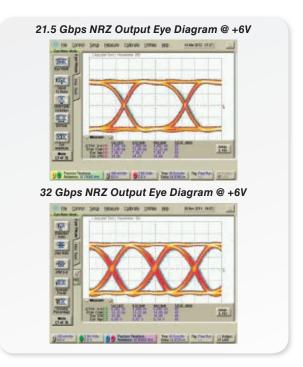
### **New & Expanded Product Lines**

### HMC5850BG 40 / 100G Optical Modulator Driver



### **Features**

- ♦ Operational to 32 Gbps: 40 Gbps DQPSK 100 Gbps DP-QPSK (Coherent) 40 Gbps DP-BPSK
- ♦ Low DC Power Dissipation: 1.4W (for 8 Vpp Swing @ 6V Supply) 0.8W (for 6 Vpp Swing @ 5V Supply)
- ♦ Small Package Size: 9.75 x 6 x 3.29 mm
- ♦ Integrated Peak Detect Feature Enables
  Monitoring & Maintaining Output Swing Stability
- ♦ Integrated Bias-Tee Feature Eliminates External Coil, Simplifies PCB Design & Lowers BOM Cost



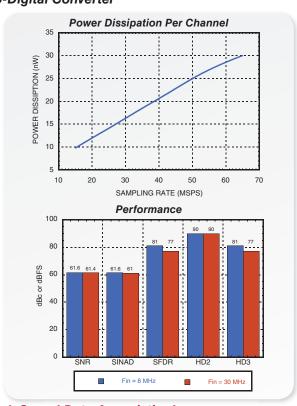
Low Power 40G / 100G Optical Modulator Driver for Long-Haul Applications! Features Integrated Bias-Tee and Peak Detection Feature!

### HMCAD1104 Octal 10-Bit 20/40/50/65 MSPS Analog-to-Digital Converter



### **Features**

- ♦ 50 MSPS Maximum Sampling Rate
- ♦ Ultra Low Power Dissipation 12 mW / Channel @ 20 MSPS 20 mW / Channel @ 40 MSPS 25 mW / Channel @ 50 MSPS 30 mW / Channel @ 65 MSPS
- ♦ 61 dB SNR @ 8 MHz Fin
- ♦ Coarse and Fine Gain Control
- ♦ 64 Lead 9 x 9 mm SMT Package



Ideal for ATE, MIMO Antennas & High Speed Data Acqusistion!



### SMT & Chip (Die) Products

### **BROADBAND TIME DELAYS - Analog & Digital**

Data / Clock Rate (Gbps / GHz)	Function	Rise / Fall (ps)	Deterministic Jitter (ps)	Differential Output Voltage Swing (Vp-p)	DC Power Consumption (mW)	Vcc Power Supply (Vdc)	Package	ECCN Code	Part Number
-/23	Analog Time Delay	10 / 11	-	0.5 - 0.95	630	+3.3	LC3	3A001.a.11.b	HMC877LC3
32 / 24	Analog Time Delay	14 / 14	6	0.15 - 0.6	1450	+3.3	LC4B	3A001.a.11.b	HMC910LC4B
32 / 24	Analog Time Delay	15 / 14	6	0.8	1600	+3.3	LC4	3A001.a.11.b	HMC911LC4B
28 / 28	5-Bit Digital Time Delay	20 / 18	< 2	0.5 - 1.35	610	-3.3	LC5	3A001.a.11.b	HMC856LC5

### **COMPARATORS** - High Speed Clocked, Latched & Window Comparators

Analog Input B/W (GHz) / Clock Rate (Gbps)	Function	Deterministic Jitter (ps)	Propagation Delay (ps)	Output Voltage Swing (Vdc)	DC Power (mW)	Vcco / V <sub>term</sub> <sup>[1]</sup> Power Supply (Vdc)	Package	ECCN Code	Part Number
10 / 20	Clocked Comparator-RSPECL	<3	120	0.4	150	+3.3 / +1.3	LC3C	3A001.a.11.b	HMC874LC3C
10 / 20	Clocked Comparator-RSCML	<3	120	0.4	130	0/0	LC3C	3A001.a.11.b	HMC875LC3C
10 / 20	Clocked Comparator-RSECL	<3	120	0.4	150	0 / -2.0	LC3C	3A001.a.11.b	HMC876LC3C
10 / [2]	Latched Comparator-RSPECL	2	85	0.4	140	+3.3 / 1.3	LC3C	3A001.a.11.b	HMC674LC3C
10 / [2]	Latched Comparator-RSPECL	2	85	0.4	140	+3.3 / 1.3	LP3	3A001.a.11.b	HMC674LP3E
10 / [2]	Latched Comparator-RSCML	2	100	0.4	100	0/0	LC3C	3A001.a.11.b	HMC675LC3C
10 / [2]	Latched Comparator-RSCML	2	100	0.4	100	0/0	LP3	3A001.a.11.b	HMC675LP3E
10 / [2]	Latched Comparator-RSECL	2	100	0.35	120	0 / -2.0	LC3C	3A001.a.11.b	HMC676LC3C
10 / [2]	Latched Comparator-RSECL	2	100	0.35	120	0 / -2.0	LP3	3A001.a.11.b	HMC676LP3E
10 / -	Window Comparator	2	88	0.4	240	+2 / 0	LC3C	3A001.a.11.b	HMC974LC3C

<sup>[1]</sup> Vee = -3.0V & Vcci = +3.3V [2] These products are pin for pin compatible

### **CROSSPOINT SWITCH**

Data / Clock Rate (Gbps / GHz)	Function	Rise / Fall Time (ps)	Deterministic Jitter (ps)	Differential Output Swing (Vp-p)	DC Power (mW)	DC Power Supply (Vdc)	Package	ECCN Code	Part Number
14 / 14	2x2 Crosspoint Switch*	21 / 21	2	0.5 - 1.2	345	-3.3	LC5	3A001.a.11.b	HMC857LC5

### **DATA CONVERTERS**

### Low Power Analog-to-Digital Converters

Sample Rate	Function / Mode	Resolution (bits)	# of Channels	Power Dissipation <sup>[2][3]</sup>	SNR (dBFS)	SFDR (dBc)	Package	ECCN Code	Part Number
640 MSPS	High Speed, Single Channel	12	1	490 mW	70	60 / 75 [1]	LP7DE	3A001.a.5.a.4	HMCAD1520
320 MSPS	High Speed, Dual Channel	12	2	490 mW	70	60 / 78 [1]		3A001.a.5.a.4	
160 MSPS	High Speed, Quad Channel	12	4	490 mW	70	60 / 78 [1]		3A001.a.5.a.4	
105 MSPS 80 MSPS	Precision, Quad Channel	14	4 4	603 mW 530 mW	74 75	83 85		3A001.a.5.a.4	
1 GSPS	High Speed, Single Channel	8	1	710 mW	49.8	49 / 64 [1]	LP7DE	3A001.a.5.a.1	HMCAD1511
500 MSPS	High Speed, Dual Channel	8	2	710 mW	49.8	44 / 63 [1]		3A001.a.5.a.1	
250 MSPS	High Speed, Quad Channel	8	4	710 mW	49.8	57 / 70 [1]		3A001.a.5.a.1	
500 MSPS	High Speed, Single Channel	8	1	295 mW	49.8	49 / 65 [1]	LP7DE	3A991.c.1	HMCAD1510
250 MSPS	High Speed, Dual Channel	8	2	295 mW	49.8	59 / 69 [1]		3A991.c.1	
125 MSPS	High Speed, Quad Channel	8	4	295 mW	49.7	60 / 69 [1]		3A991.c.1	
80 MSPS	Octal Channel	13 / 12	8	59 mW / Channel	70.1	77	LP9E	3A991.c.3	HMCAD1102
65 MSPS	Octal Channel	13 / 12	8	51 mW / Channel	72.2	82	LP9E	3A991.c.3	HMCAD1101
20/40/50/65 MSPS	Octal Channel	10	8	12/20/25/30 mW / Channel	61.6	81	LP9E	EAR99	HMCAD1104
50 MSPS	Octal Channel	13 / 12	8	41 mW / Channel	72.2	82	LP9E	3A991.c.3	HMCAD1100
40 MSPS	Octal Channel	13 / 12	8	35 mW / Channel	72.2	82		3A991.c.3	
20 MSPS	Octal Channel	13 / 12	8	23 mW / Channel	72.2	82		3A991.c.3	
80 MSPS	Dual Channel	13 / 12	2	102 mW	72	77	LP9E	3A991.c.3	HMCAD1050-8
65 MSPS	Dual Channel	13 / 12	2	85 mW	72.6	81		3A991.c.3	
40 MSPS	Dual Channel	13 / 12	2	55 mW	72.7	81	LP9E	3A991.c.3	HMCAD1050-4
20 MSPS	Dual Channel	13 / 12	2	30 mW	72.2	85		3A991.c.3	



### SMT & Chip (Die) Products

### **DATA CONVERTERS**

### Low Power Analog-to-Digital Converters

Sample Rate	Function / Mode	Resolution (bits)	# of Channels	Power Dissipation <sup>[2][3]</sup>	SNR (dBFS)	SFDR (dBc)	Package	ECCN Code	Part Number
80 MSPS	Single Channel	13 / 12	1	60 mW	72	77	LP6HE	3A991.c.3	HMCAD1051-80
65 MSPS	Single Channel	13 / 12	1	50 mW	72.6	81		3A991.c.3	
40 MSPS	Single Channel	13 / 12	1	33 mW	72.7	81	LP6HE	3A991.c.3	HMCAD1051-40
20 MSPS	Single Channel	13 / 12	1	19 mW	72.2	85		3A991.c.3	•
80 MSPS	Dual Channel	10	2	78 mW	61.6	75	LP9E	EAR99	HMCAD1040-80
65 MSPS	Dual Channel	10	2	65 mW	61.6	77		EAR99	
40 MSPS	Dual Channel	10	2	43 mW	61.6	81	LP9E	EAR99	HMCAD1040-40
20 MSPS	Dual Channel	10	2	24 mW	61.6	81		EAR99	
80 MSPS	Single Channel	10	1	46 mW	61.6	75	LP6HE	EAR99	HMCAD1041-80
65 MSPS	Single Channel	10	1	38 mW	61.6	77		EAR99	
40 MSPS	Single Channel	10	1	25 mW	61.6	81	LP6HE	EAR99	HMCAD1041-40
20 MSPS	Single Channel	10	1	15 mW	61.6	81		EAR99	
[1] Excluding Inte	rleaving Spurs.								

### **Ultra High Speed Analog-to-Digital Converters**

Freq	Input uency (GHz)	Function	Sample Rate (Gsps)	Resolution (Bits)	ENOB	SFDR (dBFS)	Package	ECCN Code	Part Number
NEW!	20	3-Bit ADC with	26	3	2.9	26	LP9	3A001.a.11.b	HMCAD5831LP9BE

### Track-and-Hold Amplifiers

Fre	Input equency (GHz)	Function	Single Tone THD/SFDR (dB)	Maximum Clock Rate (GS/s)	Output Noise (mV RMS)	Hold Mode Feed- through Rejection (dB)	Package	ECCN Code	Part Number
NEW!	DC - 5	Track-and-Hold	-65 / 67	4.0	0.86	> 60	LC4B	3A001.a.11.b	HMC760LC4B
NEW!	DC - 18	Track-and-Hold	-65 / 67	4.0	1.65	> 60	LC4B	3A001.a.11.b	HMC661LC4B
	0.02 - 4.5	Track-and-Hold	-66 / 67	3.0	0.95	> 60	LC4B	3A001.a.11.b	HMC660LC4B

### DC POWER CONDITIONING - Linear Voltage Regulators

Input Voltage (V)	Function	Output Voltage (V)	Output Current					Regulated Outputs	Package	ECCN Code	Part Number
voitage (v)		voitage (v)	(mA)	1 kHz	1 MHz	1 kHz	10 kHz	Outputs		Ooue	Number
3.35 - 5.6	Quad High PSRR	2.5 - 5.2	15 - 100	80	60	7	3	4	LP3	EAR99	HMC860LP3E
3.35 - 5.6	Low Noise, High PSRR	1.8 - 5.2	500	80	60	7	3	4	LP3	EAR99	HMC1060LP3E
4.8 to 5.6	Low Noise, High PSRR	1.8 to 5.1	400	60	30	6	3	1	LP3	EAR99	HMC976LP3E

### **DC POWER MANAGEMENT - Active Bias Controller**

v	Supply oltage Range (V)	Function	VDRAIN Voltage Range (V)	IDRAIN Bias Current (mA)	IGATE Drive Current (mA)	VGATE Voltage Range (V)	Over / Under IDRAIN Current Alarm	Low VDD Alarm	Package	ECCN Code	Part Number
	4 to 12	Active Bias Controller	4 to 12	20 to 200	-0.8 to 0.8	-2.5 to 2.0	-	-	Chip	EAR99	HMC981
	4 to 12	Active Bias Controller	4 to 12	0 to 200	-0.8 to 0.8	-2.5 to 2.5	-	-	LP3	EAR99	HMC981LP3E
	5 to 16.5	Active Bias Controller	3 to 15	0 to 500	-4 to 4	-2.5 to 2.5	Yes	Yes	LP5	EAR99	HMC920LP5E
NEW	! 5 - 16.5	Active Bias Controller	5 - 16.5	50 - 1600	-4 to 4	-2.46 to +2.04	Yes	-	Chip	EAR99	HMC980
	5 to 16.5	Active Bias Controller	5 to 16.5	50 to 1600	-4 to 4	-2.46 to +2.04	Yes	-	LP4	EAR99	HMC980LP4E

### HIGH SPEED DIGITAL LOGIC

Data / Clock Rate (Gbps / GHz)	Function	Rise / Fall Time (ps)	Deterministic Jitter (ps)	Differential Output Swing (Vp-p)	DC Power (mW)	DC Power Supply (Vdc)	Package	ECCN Code	Part Number
1:2 & 1:4 Fand	out Buffers								
13 / 13	Fast Rise Time 1:2 Fanout Buffer*	19 / 18	2	0.6 - 1.1	300	-3.3	LP3	3A001.a.11.b	HMC720LP3E
13 / 13	Fast Rise Time 1:2 Fanout Buffer	19 / 18	2	1.1	300	-3.3	LC3C	3A001.a.11.b	HMC724LC3C
13 / 13	Fast Rise Time 1:2 Fanout Buffer*	22 / 20	2	0.6 - 1.2	290	+3.3	LC3C	3A001.a.11.b	HMC744LC3C
28 / 20	1:2 Fanout Buffer*	16 / 15	2	0.6 - 1.1	315	-3.3	LC3C	3A001.a.11.b	HMC850LC3C
45 / 28	1:2 Fanout Buffer*	11 / 11	3	0.4 - 1.2	465	-3.3	LC4B	3A001.a.11.b	HMC842LC4B
13 / 13	1:4 Fanout Buffer*	26 / 25	4	0.6 - 1.4	440	-3.3	LC4B	3A001.a.11.b	HMC940LC4B
			<u>_</u>	*** ***					



### SMT & Chip (Die) Products

### HIGH SPEED DIGITAL LOGIC

Data / Clock Rate (Gbps / GHz)	Function	Rise / Fall Time (ps)	Deterministic Jitter (ps)	Differential Output Swing (Vp-p)	DC Power (mW)	DC Power Supply (Vdc)	Package	ECCN Code	Part Number
2:1 Selectors									
14 / 14	2:1 Differential Selector*	19 / 20	2	0.5 - 1.3	221	-3.3	LC4B	3A001.a.11.b	HMC858LC4B
13 / 13	2:1 Selector*	22 / 22	2	0.6 - 1.2	250	+3.3	LC3C	3A001.a.11.b	HMC748LC3C
14 / 14	4:1 Selector*	17 / 17	2	0.5 - 1.3	294	-3.3	LC5	3A001.a.11.b	HMC958LC5
AND / NAND /	OR / NORs								
13 / 13	Fast Rise Time AND / NAND / OR / NOR*	19 / 18	2	0.6 - 1.1	230	-3.3	LP3	3A001.a.11.b	HMC722LP3E
13 / 13	Fast Rise Time AND / NAND / OR / NOR	19 / 18	2	1.1	230	-3.3	LC3C	3A001.a.11.b	HMC726LC3C
13 / 13	Fast Rise Time AND / NAND / OR / NOR*	22 / 21	2	0.6 - 1.2	230	+3.3	LC3C	3A001.a.11.b	HMC746LC3C
28 / 28	AND / NAND / OR / NOR*	15 / 14	2	0.6 - 1.5	241	-3.3	LC3C	3A001.a.11.b	HMC852LC3C
45 / 25	AND / NAND / OR / NOR*	10 / 10	2	0.2 - 0.9	530	-3.3	LC4B	3A001.a.11.b	HMC843LC4B
Clock Divider	rs								
- / 26	Clock Divide-by-4*	19 / 19	-	0.8 - 1.8	281	-3.3	LC3	3A001.a.11.b	HMC959LC3
- / 26	Clock Divide-by-8*	19 / 17	-	0.8 - 1.8	520	-3.3	LC3	3A001.a.11.b	HMC859LC3
D-Type Flip-F	lops								
14 / 14	Dual D-Type Flip-Flop with Common Clock*	22 / 20	2	0.6 - 1.3	442	-3.3	LC4B	3A001.a.11.b	HMC953LC4B
13 / 13	Fast Rise Time D-Type Flip-Flop*	19 / 17	2	0.7 - 1.3	260	-3.3	LC3C	3A001.a.11.b	HMC723LP3E
13 / 13	Fast Rise Time D-Type Flip-Flop	19 / 17	2	1.1	260	-3.3	LC3C	3A001.a.11.b	HMC727LC3C
13 / 13	Fast Rise Time D-Type Flip-Flop*	22 / 20	2	0.7 - 1.2	264	+3.3	LC3C	3A001.a.11.b	HMC747LC3C
28 / 28	D-Type Flip-Flop*	15 / 14	2	0.7 - 1.3	260	-3.3	LC3C	3A001.a.11.b	HMC853LC3C
43 / 43	D-Type Flip-Flop*	12 / 12	2	0.2 - 0.85	630	-3.3	LC4B	3A001.a.11.b	HMC841LC4B
NRZ-to-RZ Co	onverters								
13 / 13	NRZ-to-RZ Converter	15 / 13	2	0.3 - 1.2	594	+3.3	LC3C	3A001.a.11.b	HMC706LC3C
T Flip-Flops									
26 / 26	T Flip-Flop w/ Reset*	18 / 17	2	0.6 - 1.2	270	+3.3	LC3C	3A001.a.11.b	HMC749LC3C
XOR / XNORs	<b>;</b>								
13 / 13	Fast Rise Time XOR / XNOR*	19 / 18	2	0.6 - 1.2	230	-3.3	LP3	3A001.a.11.b	HMC721LP3E
13 / 13	Fast Rise Time XOR / XNOR	19 / 18	2	1.1	230	-3.3	LC3C	3A001.a.11.b	HMC725LC3C
13 / 13	Fast Rise Time XOR / XNOR*	21 / 19	2	0.6 - 1.2	240	+3.3	LC3C	3A001.a.11.b	HMC745LC3
28 / 28	XOR / XNOR*	15 / 14	2	0.6 - 1.4	241	-3.3	LC3C	3A001.a.11.b	HMC851LC3C
45 / 28	XOR / XNOR*	11 / 10	3	0.2 - 8.5	512	-3.3	LC4B	3A001.a.11.b	HMC844LC4B
* These product	s feature programmable output volt	age swing.							

### 1:9 Fanout Buffer

Clock Rate (GHz)	Function	Input	Output	Phase Jitter (12 k to 20 MHz)	Rise/Fall Time (ps)	Channel Skew (ps)	Disable Mode	Power Supply (V)	Package	ECCN Code	Part Number
DC - 8	1:9 Fanout Buffer	LVPECL, LVDS, CML, CMOS	LVPECL	8 fs RMS	65	3.1	Yes	3.3	LP5	3A001.a.11.b	HMC987LP5E

### IF / BASEBAND PROCESSING - Dual Baseband Low Pass Filter & Dual Baseband Digital VGA

### **Dual Baseband Low Pass Filter**

3 dB Bandwidth Setting (MHz)	Function	3 dB Bandwidth Accuracy (%)	Gain (dB)	NF (dB)	OIP3 (dBm)	Package	ECCN Code	Part Number
3.5 - 50	Dual Low Pass with ADC Driver	±2.5	0 / 10	12	30	LP5	EAR99	HMC900LP5E

### **Dual Baseband Digital VGA**

	quency MHz)	Function						Magnitude (dB) / Phase (deg) Balance	Bias Supply	Package	ECCN Code	Part Number
DC	C - 100	Digital, Serial & Parallel Control	6	0 to 40	+30	+65	55	±0.1 / ±1	+5V @ 70 mA	LP4	EAR99	HMC960LP4E



### **Analog-to-Digital Conversion**

### INTERFACE - RF Switch, Attenuator & Phase Shifter Digital Drivers

Bit Rate (mbps)	Function	Input	Output Voltage (V)	Output Current (mA)	Bias Supply	Package	ECCN Code	Part Number
10	6-Bit Switch Driver / Controller	TTL/CMOS	-5 / +2.2	1	+5V @ 1.5 mA	LP5	EAR99	HMC677LP5E
10	6-Bit Switch Driver / Controller	TTL/CMOS	-5 / +2.2	1	+5V @ 1 mA	G32	EAR99	HMC677G32

### **LIMITING AMPLIFIERS**

Data Rate (Gbps)	Function	Small Signal Bandwidth (GHz)	Differential Gain (dB)	Deterministic Jitter (ps p-p)	Additive Random Jitter (ps rms)	Supply Current	Package	ECCN Code	Part Number
12.5	Limiting Amplifier	11	44	5	0.2	+5V @ 106 mA	LP4	EAR99	HMC750LP4E
12.5	Limiting Amplifier with LOS	9.5	32	-	0.9	+3.3V @ 47 mA	LP4	EAR99	HMC914LP4E
32	Limiting with DC Offset	25	30	5	0.3	+3.3V @ 90 mA	LC3C	EAR99	HMC865LC3C
32	Limiting without DC Offset	25	29	7	0.3	+3.3V @ 85 mA	LC3C	EAR99	HMC866LC3C

### **MUX & DEMUX**

Data / Clock Rate (Gbps / GHz)	Function	Rise / Fall (ps)	Deterministic Jitter (ps)	Differential Output Voltage Swing (Vp-p)	DC Power Consumption (mW)	Vee Power Supply (Vdc)	Package	ECCN Code	Part Number
32 / 16	2:1 Mux*	15 / 15	-	1.25	480	±3.3	LC4B	3A001.a.11.b	HMC954LC4B
28 / 14	4:1 Mux with Adj. Vout	16 / 16	4	0.7 - 1.25	510	-3.3	LC5	3A001.a.11.b	HMC854LC5
45 / 22.5	4:1 Mux*	11 / 12	3	0.25 - 0.9	1782	+3.3	LC5	3A001.a.11.b	HMC847LC5
32 / 16	1:2 Demux with High Speed Invert*	19 / 18	< 3	1.0	644	±3.3	LC4B	3A001.a.11.b	HMC955LC4B
28 / 14	1:4 Demux with Adj. Vout	22 / 22	-	0.45 - 1.14	644	-3.3	LC5	3A001.a.11.b	HMC855LC5
45 / 22.5	1:4 Demux with Adj. Vout	25 / 21	4	0.3 - 1.0	1782	+3.3	LC5	3A001.a.11.b	HMC848LC5

<sup>\*</sup> With Programmable Output Voltage and/or Duty Cycle Control

### **OPTICAL MODULATOR DRIVERS**

Data Rate Max. (Gbps)	Function	Gain (dB)	Group Delay Variation (ps)	Additive Jitter (ps)	Output Voltage Max. (Vp-p)	Package	ECCN Code	Part Number
22.5	8Vpp Optical Modulator Driver	18	±15	0.3	8	LC5	EAR99	HMC870LC5 [1]
22.5	3Vpp Optical Modulator Driver	15	±15	0.3	3	LC5	EAR99	HMC871LC5 [1]
32	3Vpp Optical Modulator Driver, with Peak Detect	14	±5	0.3	3	Chip	EAR99	HMC1050 <sup>[1][2]</sup>
32	8Vpp Optical Modulator Drive, with Peak Detect	16	±5	0.3	8	Chip	EAR99	HMC1051 [1] [2]
<b>W!</b> 32	8Vpp Optical Modulator Driver, SMT Package	32	±7	0.25	8	BGA	EAR99	HMC5850BG <sup>[1]</sup> <sup>[2]</sup>

<sup>[1]</sup> Drivers that benefit from Hittite Active Bias Controllers [2] Request Data Sheet: FO@hittite.com

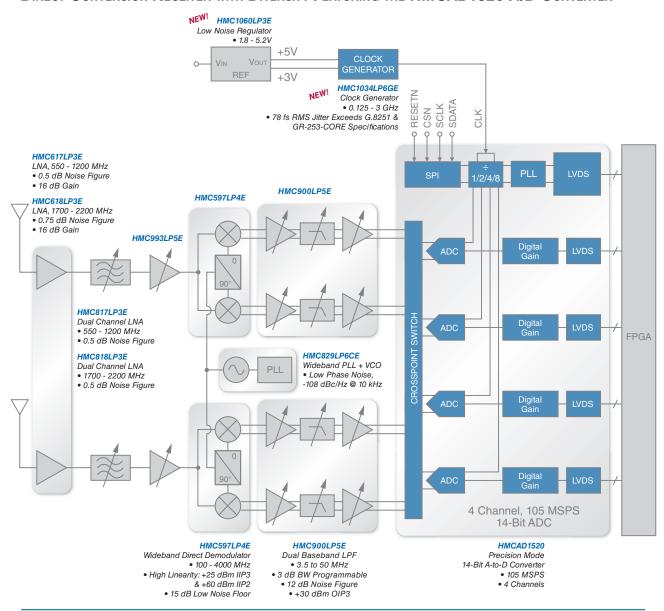
### TRANSIMPEDANCE AMPLIFIERS

Data Rate (Gbps)	Function	Transimpedance (kΩ)	Input Overload (mApp)	Small Signal Bandwidth (GHz)	Deterministic Jitter (ps)	Noise (pA/√Hz)	Package	ECCN Code	Part Number
0.1 - 1.0	Low Noise Transimpedance Amplifier	10	20	0.7	< 100	4.6	LP3	EAR99	HMC799LP3E
1 - 10	Transimpedance Amplifier	1.25	3	7.5	< 10	11	Chip	EAR99	HMC690

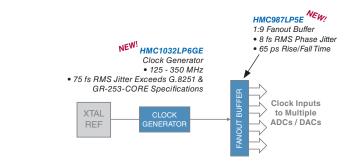


### **Baseband and Zero IF Communication**

### DIRECT CONVERSION RECEIVER WITH DIVERSITY FEATURING THE HMCAD1520 A/D CONVERTER



### ADC / DAC CLOCK DRIVER CIRCUIT



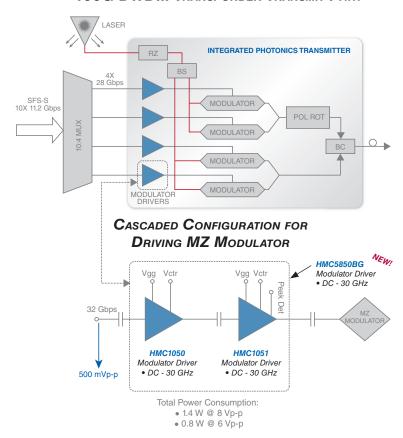
Typical Fiber Optic & Networking applications are illustrated.

See the full product listing for alternatives to the select HMC products shown in each functional block.

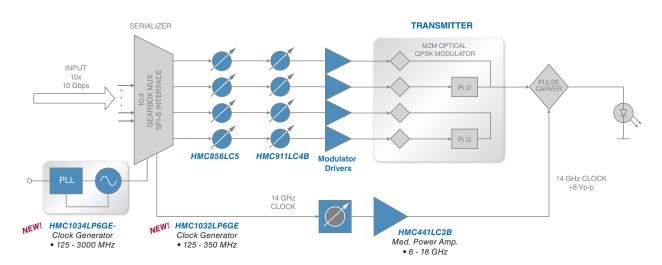


### **Fiber Optics & Networking**

### 100G DWDM TRANSPONDER TRANSMIT PATH



### CASCADED CONFIGURATION FOR DRIVING MZ MODULATOR



Typical Fiber Optic & Networking applications are illustrated.

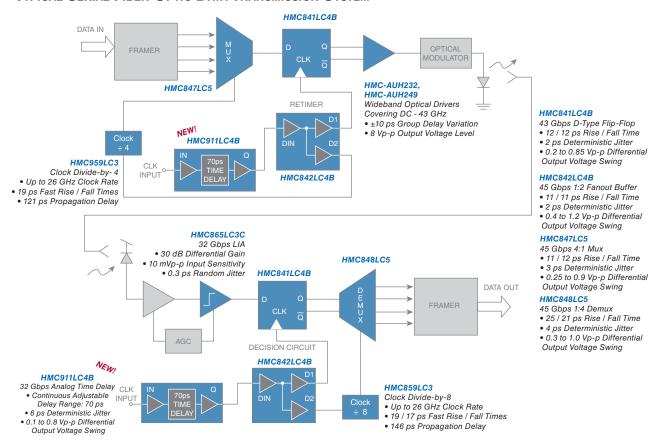
See the full product listing for alternatives to the select HMC products shown in each functional block.

### Market & Application Guide



### **Fiber Optics & Networking**

### TYPICAL SERIAL FIBER OPTIC DATA TRANSMISSION SYSTEM



### 43 GBPS HOGGE PHASE DETECTOR FOR CLOCK & DATA RECOVERY

#### HMC-C064 50 Gbps XOR / XNOR • 6.5 / 10 ps Rise / Fall Time HMC-C064 • 2 ps Deterministic Jitter 0.5 Vp-p Differential Output Voltage Swing DATA INPUT DATA OUTPUT HMC-C060 HMC-C060 43 Gbps D-Type Flip-Flop • 9 / 10 ps Rise / Fall Time • 1.5 ps Deterministic Jitter • 0.5 Vp-p Differential Output Voltage Swing HMC-C062 50 Gbps 1:2 Fanout Buffer • 9.5 / 11 ps Rise / Fall Time 2 ps Deterministic Jitter CLK INPUT • 0.5 Vp-p Differential Output Voltage Swing HMC-C073 VCO + Buffer Amn • 38.4 - 43.2 GHz Fo Low Phase Noise -98 dBc/Hz @ 100 kHz • +5V @ 350 mA

### 13 GBPS, NRZ-TO-RZ CONVERSION

### HMC706LC3C 13 Gbps NRZ-to-RZ Converter 15 / 13 ps Rise / Fall Time • 2 ps Deterministic Jitter • 0.3 to 1.2 Vp-p Differential FIBER Output Voltage Swing NRZ HMC870LC5 MZ Optical Modulator Driver • DC - 20 GHz • ±15 ps Group Delay Variation • 2.5 to 8 Vp-p Output Voltage Level INPUT HMC720LP3E 13 Gbps 1:2 Fanout Buffer • 19 / 18 ps Rise / Fall Time • 2 ps Deterministic Jitter • 0.6 to 1.1 Vp-p Differential Output Voltage Swing



### CLOCKS & TIMING ICS

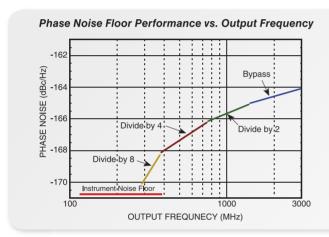
### **New & Expanded Product Lines**

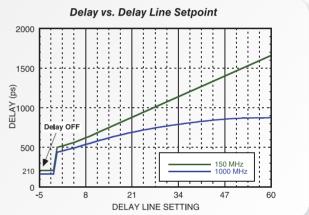
### HMC988LP3E Programmable Clock Divider and Delay Management IC



#### **Features**

- ♦ Programmable Clock Divide by 1/2/4/8/16/32
- ♦ Delay Adjustment in Multiples of 1/2 Clock Cycles or in 60 Steps of 20 ps (Typ.)
- ♦ -170 dBc/Hz Noise Floor @ 100 MHz Output
- ♦ Up to 4 GHz Operation with 800 mVp-p LVPECL Output
- ♦ 3.3V Operation (or 5V Operation with Optional On-Chip Regulator for Best Performance)





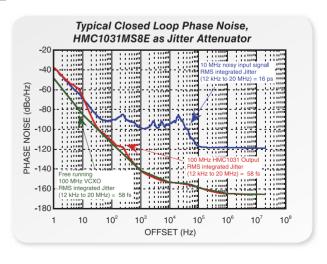
Ideal for Data Converter Sample Clock Phase Adjustment in Basestation, ATE and Networking Applications!

### HMC1031MS8E Clock Generator with Integer-N PLL



#### **Features**

- ♦ Integer-N PLL Clock Generator with External VCO/VCXO
- ♦ Ultra-Low Power Consumption: <2 mA Typical in Normal Operation
- ♦ Output Frequency: Up to 500 MHz
- ♦ Hardware Pin Programmable Reference Clock Multiplication Ratios of x1, x5 and x10
- ♦ Phase Noise Floor (Figure of Merit): -208 dBc/Hz (Typ.)



Ultra-Low Power Integer PLL Clock Generator for Jitter Attenuation and Frequency Translation!





### SMT & Chip (Die) Products

#### **CLOCKS & TIMING**

#### **Clock Distribution**

	Max. Clock Rate (GHz)	Function	Input	Output	Phase Jitter (12 k to 20 MHz)	Rise/Fall Time (ps)	Channel Skew (ps)	Disable Mode	Power Supply (V)	Package	ECCN Code	Part Number
NEW	! 4	Clock Divider & Delay Management	LVPECL, LVDS, CML, CMOS	LVPECL	13 fs RMS	90	300 to 1500	Yes	5 or 3.3	LP3	3A001.a.11.b	HMC988LP3E
	8	1:9 Fanout Buffer	LVPECL, LVDS, CML, CMOS	LVPECL	8 fs RMS	65	3.1	Yes	3.3	LP5	3A001.a.11.b	HMC987LP5E

#### **Clock Generators**

	Max. Frequency (MHz)	Function		Phase Noise Floor (dBc/Hz)	Maximum Reference Freq. (MHz)	Typical Power I Consumption (W)	Figure of Merit (Frac/Int) (dBc/Hz)	Package	ECCN Code	Part Number
NEW!	500	Integer Mode PLL (x1, x5, x10)	Defined by VCXO	Defined by VCXO	140	0.0064	-208	MS8	EAR99	HMC1031MS8E
	350	Clock Generator with Fractional-N PLL+VCO	116 / 75	-165	350	0.86	-227 / -230	LP6G	3A001.a.11.b	HMC1032LP6GE
_	3000	Clock Generator with	118 / 78	-165	350	0.86	-227 / -230	LP6G	3A001.a.11.b	HMC1034LP6GE

PLLs with INTEGRATED VCOs - RF & Wideband PLLs with Integrated VCOs

Frequency (MHz)	Function	Closed Loop SSB Phase Noise @ 10 kHz Offset	Open Loop VCO Phase Noise @ 1 MHz Offset	Pout (dBm)	RMS Jitter Fractional Mode (fs)	Integrated PN Fractional Mode (deg rms)	Package	ECCN Code	Part Number
fo/2									
665 - 825	Tri-Band RF VCO	-118 dBc/Hz	-148 dBc/Hz	11	180	0.05	LP6C	3A001.a.11.b	HMC822LP6CE
795 - 945	Tri-Band RF VCO	-123 dBc/Hz	-148 dBc/Hz	10	180	0.06	LP6C	3A001.a.11.b	HMC838LP6CE
780 - 870	RF VCO	-116 dBc/Hz	-148 dBc/Hz	14	180	0.06	LP6C	3A001.a.11.b	HMC824LP6CE
860 - 1040	Tri-Band RF VCO	-118 dBc/Hz	-147 dBc/Hz	10	180	0.07	LP6C	3A001.a.11.b	HMC821LP6CE
990 - 1105	RF VCO	-114 dBc/Hz	-146 dBc/Hz	11	180	0.07	LP6C	3A001.a.11.b	HMC826LP6CE
1025 - 1150	Tri-Band RF VCO	-123 dBc/Hz	-147 dBc/Hz	12	180	0.07	LP6C	3A001.a.11.b	HMC837LP6CE
1050 - 1205	Tri-Band RF VCO	-121 dBc/Hz	-146 dBc/Hz	10	180	0.08	LP6C	3A001.a.11.b	HMC839LP6CE
1095 - 1275	Tri-Band RF VCO	-118 dBc/Hz	-147 dBc/Hz	10	180	0.08	LP6C	3A001.a.11.b	HMC820LP6CE
1310 - 1415	Tri-Band RF VCO	-121 dBc/Hz	-145 dBc/Hz	10	180	0.09	LP6C	3A001.a.11.b	HMC840LP6CE
fo									
1285 - 1415	RF VCO	-112 dBc/Hz	-143 dBc/Hz	10	180	0.09	LP6C	3A001.a.11.b	HMC828LP6CE
1330 - 1650	Tri-Band RF VCO	-112 dBc/Hz	-142 dBc/Hz	6.5	180	0.11	LP6C	3A001.a.11.b	HMC822LP6CE
1590 - 1890	Tri-Band RF VCO	-118 dBc/Hz	-143 dBc/Hz	7.5	180	0.12	LP6C	3A001.a.11.b	HMC838LP6CE
1720 - 2080	Tri-Band RF VCO	-112 dBc/Hz	-141 dBc/Hz	6.5	180	0.13	LP6C	3A001.a.11.b	HMC821LP6CE
1815 - 2010	RF VCO	-112 dBc/Hz	-143 dBc/Hz	7.5	180	0.13	LP6C	3A001.a.11.b	HMC831LP6CE
2050 - 2300	Tri-Band RF VCO	-117 dBc/Hz	-141 dBc/Hz	10.5	180	0.15	LP6C	3A001.a.11.b	HMC837LP6CE
2100 - 2410	Tri-Band RF VCO	-115 dBc/Hz	-140 dBc/Hz	7.5	180	0.16	LP6C	3A001.a.11.b	HMC839LP6CE
2190 - 2550	Tri-Band RF VCO	-112 dBc/Hz	-141 dBc/Hz	6.5	180	0.17	LP6C	3A001.a.11.b	HMC820LP6CE
2620 - 2830	Tri-Band RF VCO	-115 dBc/Hz	-139 dBc/Hz	9	180	0.18	LP6C	3A001.a.11.b	HMC840LP6CE
2fo									
2660 - 3300	Tri-Band RF VCO	-106 dBc/Hz	-136 dBc/Hz	-4	180	0.21	LP6C	3A001.a.11.b	HMC822LP6CE
3180 - 3780	Tri-Band RF VCO	-112 dBc/Hz	-135 dBc/Hz	-4	180	0.24	LP6C	3A001.a.11.b	HMC838LP6CE
3365 - 3705	RF VCO	-107 dBc/Hz	-135 dBc/Hz	0	190	0.25	LP6C	3A001.a.11.b	HMC836LP6CE
3440 - 4160	Tri-Band RF VCO	-106 dBc/Hz	-135 dBc/Hz	-4	180	0.27	LP6C	3A001.a.11.b	HMC821LP6CE
4100 - 4600	Tri-Band RF VCO	-111 dBc/Hz	-135 dBc/Hz	-0.5	180	0.30	LP6C	3A001.a.11.b	HMC837LP6CE
4200 - 4820	Tri-Band RF VCO	-108 dBc/Hz	-135 dBc/Hz	-4	180	0.31	LP6C	3A001.a.11.b	HMC839LP6CE
4380 - 5100	Tri-Band RF VCO	-106 dBc/Hz	-135 dBc/Hz	-4	180	0.33	LP6C	3A001.a.11.b	HMC820LP6CE
5240 - 5660	Tri-Band RF VCO	-109 dBc/Hz	-133 dBc/Hz	-3	180	0.37	LP6C	3A001.a.11.b	HMC840LP6CE
Wideband Cont	inuous Tuning								
25 - 3000	Wideband RF VCO	-114 dBc/Hz @ 2 GHz	-141 dBc/Hz @ 2 GHz	5	82 [1]	0.114 @ 2 GHz	LP6G	3A001.a.11.b	HMC830LP6GE
25 - 6000	Wideband RF VCO	-108 dBc/Hz @ 4 GHz	-135 dBc/Hz @ 4 GHz	-4	82 [1]	0.22 @ 4 GHz	LP6G	3A001.a.11.b	HMC833LP6GE
45 - 1050 1400 - 2100 2800 - 4200 Fo	Wideband RF VCO	-108 dBc/Hz @ 4 GHz	-134 dBc/Hz @ 4 GHz	4	82 [1]	0.229 @ 4 GHz	LP6G	3A001.a.11.b	HMC829LP6GE
45 - 1050 1400 - 2100 2800 - 4200 Fo 5600 - 8400	Wideband RF VCO	-102 dBc/Hz @ 8 GHz	-128 dBc/Hz @ 8 GHz	5 2 2 -10	82 [1]	0.43 @ 8 GHz	LP6G	3A001.a.11.b	HMC834LP6GE

Please note the DC Power Conditioning Table is in the LO Generation ICs Section.

<sup>[1]</sup> RMS Jitter Integration Bandwidth from 12 kHz to 20 MHz \*Please note the DC Power Conditioning Table is in the LO Generation ICs Section.

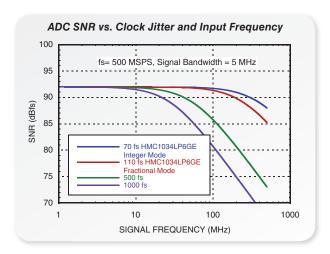


## MARKET & APPLICATION GUIDE

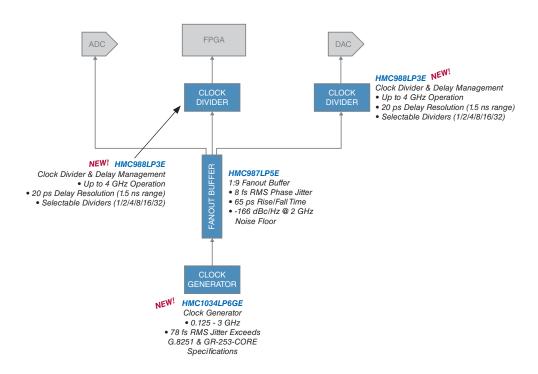
### **Clock Generators for Data Converters Clocking**

#### EXTRACT THE BEST SNR PERFORMANCE FROM YOUR DATA CONVERTERS!

- ♦ HMC1034LP6GE achieves <100 fs RMS Phase Jitter in Integer Mode
- ♦ HMC987LP5E, 1:8 LVPECL Fan-Out Buffer Distributes Data Converter Sample Clocks with Only 8 fs RMS Additive Jitter (12 kHz 20 MHz)
- ♦ HMC988LP3E Clock Divider & Delay Management IC Adjusts Data Converter Sample Clock Windows in 20 ps Resolution and Offers -170 dBc/Hz Phase Noise Floor



The low phase noise floor of a clock signal as well as its low integrated phase jitter helps to minimize the SNR degradation at high ADC / DAC input frequencies in multi-carrier, multi-acquisition applications. Hittite's Clock & Timing ICs are designed with data converter applications in mind, and work well with Hittite's High-Speed ADC devices.



## MARKET & APPLICATION GUIDE

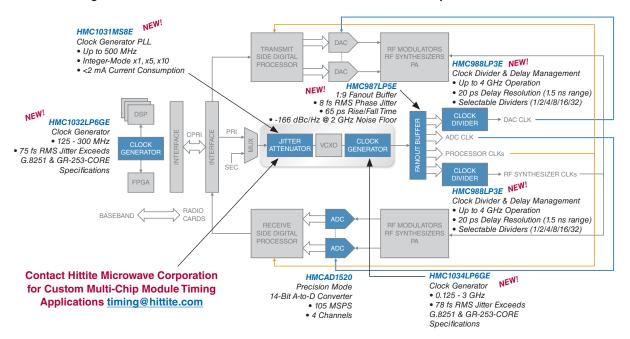


#### **Clocks & Timing**

FOR BROADBAND, CELLULAR INFRASTRUCTURE AND FIBER OPTIC & NETWORKING

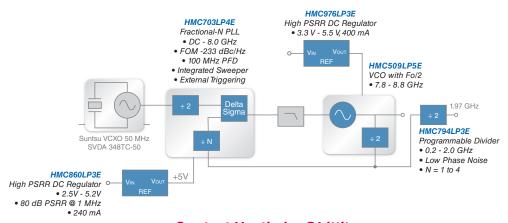
#### **Features**

- ♦ Low Noise Floor of -166 dBc/Hz Makes the HMC987LP5E Ideal for Clocking High Performance ADC/DAC & SERDES Devices
- ♦ HMC1031MS8E Ultra-Low Power Integer Mode PLL Enables Jitter Attenuation with 1.6 mA Typical Current Consumption from a Single 3.3V Supply
- ♦ HMC988LP3E Offers Selectable Frequency Division and Clock Delay Management with 20 ps Resolution Up to 1.5 ns Total Delay Range
- ♦ <100 fs Integrated Phase Jitter of the HMC1031LPGE Clock Generator Improves Data Converter SNR



Contact Us: timing@hittite.com

#### REFERENCE CLOCK SOLUTIONS FOR 100G DP-QPSK



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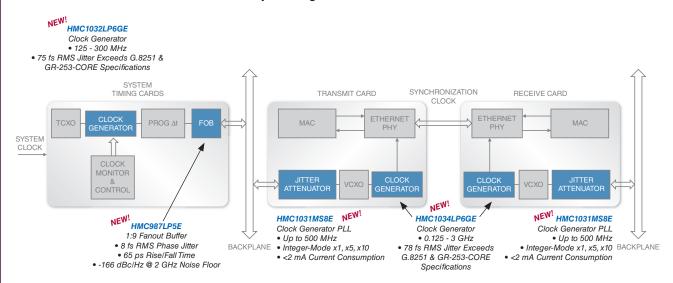
## MARKET & APPLICATION GUIDE

**Clocks & Timing** 

#### FOR BROADBAND, CELLULAR INFRASTRUCTURE AND FIBER OPTIC & NETWORKING

#### **Features**

- ♦ <10 fs 12 kHz 20 MHz integrated Phase Jitter Performance of HMC987LP5E Enables High Performance Clock Distribution With Negligible Jitter Generation
- ♦ A Flexible Input Interface Allows The HMC987LP5E LVDS, CML & CMOS Inputs to 8 LVPECL Outputs
- ♦ HMC1034LP6GE May Be Used For Clock Generation & Fractional Multiplication With Outputs Up to 3 GHz
- ♦ The HMC1034LP6GE Achieves Industry Leading Phase Jitter of 78 fs RMS



Contact Us: timing@hittite.com



## SMT & Chip (Die) Products

#### DC POWER CONDITIONING - Linear Voltage Regulators

Input Voltage (V)	Function	Output Voltage (V)	Output Current (mA)	Power Suppl Ratio (PS 1 kHz		Output Nois Density 1 kHz			Package	ECCN Code	Part Number
3.35 - 5.6	Quad High PSRR	2.5 - 5.2	15 - 100	80	60	7	3	4	LP3	EAR99	HMC860LP3E
3.35 - 5.6	Low Noise, High PSRR	1.8 - 5.2	500	80	60	7	3	4	LP3	EAR99	HMC1060LP3E
4.8 to 5.6	Low Noise, High PSRR	1.8 to 5.1	400	60	30	6	3	1	LP3	EAR99	HMC976LP3E

#### FILTERS - Tunable

NE

#### Programmable Harmonic

	Frequency Range (GHz)	Function	Return Loss (dB)	3 dB Bandwidth (GHz)	Stopband Frequency (Rej. >10 dB)	Tuning Response (ns)	Package	ECCN Code	Part Number
EW!	DC - 9	Programmable Harmonic Low Pass	10	1 - 3	1.2 Fcutoff	10	LP3	EAR99	HMC1044LP3E

#### FREQUENCY DIVIDERS (PRESCALERS) & DETECTORS

#### Frequency Dividers & Phase / Frequency Detectors

Input Frequency (GHz)	Function	Input Power (dBm)	Output Power (dBm)	100 kHz SSB Phase Noise (dBc/Hz)	Bias Supply	Package	ECCN Code	Part Number
DC - 8	Divide-by-2	-12 to +12	-6	-148	+3V @ 42 mA	SOT26	3A001.a.11.b	HMC432E
DC - 10	Divide-by-2	-15 to +10	3	-148	+5V @ 83 mA	S8G	3A001.a.11.b	HMC361S8GE
DC - 11	Divide-by-2	-15 to +10	3	-148	+5V @ 105 mA	Chip	3A001.a.11.b	HMC361
DC - 12.5	Divide-by-2	-15 to +10	2	-145	+5V @ 105 mA	S8G	3A001.a.11.b	HMC364S8GE
DC - 13	Divide-by-2	-15 to +10	3	-148	+5V @ 84 mA	G8	3A001.a.11.b	HMC361G8
DC - 13	Divide-by-2	-15 to +10	1	-145	+5V @ 105 mA	Chip	3A001.a.11.b	HMC364
DC - 13	Divide-by-2	-15 to +10	5	-145	+5V @ 110 mA	G8 Hermetic	3A001.a.11.b	HMC364G8
DC - 18	Divide-by-2	-15 to +10	-4	-150	+5V @ 77 mA	LP3	3A001.a.11.b	HMC492LP3E
DC - 7	Divide-by-3	-12 to +12	-2	-153	+5V @ 69 mA	MS8G	3A001.a.11.b	HMC437MS8GE
DC - 4	Divide-by-4	-15 to +10	3.5	-146	+3V @ 13 mA	MS8	3A001.a.11.b	HMC426MS8E
DC - 8	Divide-by-4	-12 to +12	-3	-150	+3V @ 53 mA	SOT26	3A001.a.11.b	HMC433E
DC - 11	Divide-by-4	-15 to +10	-6	-149	+5V @ 68 mA	Chip	3A001.a.11.b	HMC362
DC - 12	Divide-by-4	-15 to +10	-6	-149	+5V @ 68 mA	S8G	3A001.a.11.b	HMC362S8GE
DC - 13	Divide-by-4	-15 to +10	2	-151	+5V @ 110 mA	Chip	3A001.a.11.b	HMC365
DC - 13	Divide-by-4	-15 to +10	7	-151	+5V @ 120 mA	G8 Hermetic	3A001.a.11.b	HMC365G8
DC - 13	Divide-by-4	-15 to +10	2	-151	+5V @ 110 mA	S8G	3A001.a.11.b	HMC365S8GE
DC - 18	Divide-by-4	-15 to +10	-4	-150	+5V @ 96 mA	LP3	3A001.a.11.b	HMC493LP3E
10 - 26	Divide-by-4	-15 to +10	-4	-150	+5V @ 96 mA	LC3	3A001.a.11.b	HMC447LC3
DC - 7	Divide-by-5	-12 to +12	-1	-153	+5V @ 80 mA	MS8G	3A001.a.11.b	HMC438MS8GE
DC - 8	Divide-by-8	-5 to +12	-2	-150	+3V @ 62 mA	SOT26	3A001.a.11.b	HMC434E
DC - 12	Divide-by-8	-15 to +10	-9	-153	+5V @ 70 mA	Chip	3A001.a.11.b	HMC363
DC - 12	Divide-by-8	-15 to +10	4	-153	+5V @ 90 mA	G8 Hermetic	3A001.a.11.b	HMC363G8
DC - 12	Divide-by-8	-15 to +10	-9	-153	+5V @ 70 mA	S8G	3A001.a.11.b	HMC363S8GE
DC - 18	Divide-by-8	-15 to +10	-4	-150	+5V @ 105 mA	LP3	3A001.a.11.b	HMC494LP3E
0.1 - 6.5	Programmable Divider (N = 1 to 17)	-15 to +10	0	-153	+5V @ 200 mA	LP4	3A001.a.11.b	HMC705LP4E
0.1 - 13.0	Programmable Divider (N = 1, 3)	-10 to +10	2	-152	+5V @ 185 mA	LP3	3A001.a.11.b	HMC861LP3E
0.1 - 15	Programmable Divider (N = 1, 2, 4, 8)	-15 to 10	2	-153	+5V @ 105 mA	LP3	3A001.a.11.b	HMC862LP3E
0.2 - 2.0	Programmable Divider (N = 1 to 4)	-2 to +10	10	-160	+5V @ 135 mA	LP3	3A001.a.11.b	HMC794LP3E
0.4 - 6.0	Programmable Divider (N = 1 to 4)	0 to +9	5	-156	+3.3V @ 100 mA	LP3	3A001.a.11.b	HMC905LP3E
DC - 2.2	5-bit Counter, ÷2 to 32	-15 to +10	4	-153	+5V @ 194 mA	LP4	3A001.a.11.b	HMC394LP4E
0.01 - 1.3	Phase Frequency Detector	-10 to +10	2 Vp-p	-153	+5V @ 96 mA	QS16G	3A001.a.11.b	HMC439QS16GE

#### Fractional Divider & Frequency Detector

Input Frequency (GHz)	Function	Input Power (dBm)	Output Level (dBm)	Floor FOM (dBc/Hz)	Bias Supply	Package	ECCN Code	Part Number
DC - 7	48-Bit Delta Sigma Programmable Fractional Divider with Sweeper	-15 to -3	0.75 Vp-p to 2 Vp-p into 100 Ohm	-160	+5V @ 1 mA +3V @ 244 mA	LP5	3A001.a.11.b	HMC983LP5E
DC - 0.35	Frequency Detector & Charge Pump	3 to 15	0.02 to 2.5 mA	-231	+5V @ 97 mA +3V @ 27 mA	LP4	EAR99	HMC984LP4E

#### FREQUENCY MULTIPLIERS - Active

Input Frequency (GHz)	Function	Output Frequency (GHz)	Input Power (dBm)	Output Power (dBm)	100 kHz SSB Phase Noise (dBc/Hz)	Package	ECCN Code	Part Number
3 - 4	x2 Active	6 - 9	0	17	-140	LP4	EAR99	HMC575LP4E
4.0 - 10.5	x2 Active	8 - 21	5	17	-139	Chip	EAR99	HMC561
4.0 - 10.5	x2 Active	8 - 21	5	14	-139	LP3	EAR99	HMC561LP3E
4 - 11	x2 Active	8 - 22	5	12	-134	LC3B	EAR99	HMC573LC3B
4.5 - 8.0	x2 Active	9 - 16	2	15	-140	LP4	EAR99	HMC368LP4E
4.95 - 6.35	x2 Active	9.9 - 12.7	0	4	-142	LP3	EAR99	HMC369LP3E
6.5 - 12.3	x2 Active	13.0 - 24.6	4	17	-136	Chip	EAR99	HMC814



## SMT & Chip (Die) Products

#### FREQUENCY MULTIPLIERS - Active

Input Frequency (GHz)	Function	Output Frequency (GHz)	Input Power (dBm)	Output Power (dBm)	100 kHz SSB Phase Noise (dBc/Hz)	Package	ECCN Code	Part Number
6.5 - 12.3	x2 Active	13.0 - 24.6	4	17	-136	LC3B	EAR99	HMC814LC3B
9.0 - 14.5	x2 Active	18 - 29	3	17	-132	Chip	EAR99	HMC576
9.0 - 14.5	x2 Active	18 - 29	3	15	-132	LC3B	EAR99	HMC576LC3B
9.5 - 12.5	x2 Active	19 - 25	0	11	-135	Chip	EAR99	HMC448
10.0 - 12.5	x2 Active	20 - 25	0	11	-135	LC3B	EAR99	HMC448LC3B
11 - 23	x2 Active	22 - 46	5	15	-	Chip	EAR99	HMC598
12.0 - 16.5	x2 Active	24 - 33	3	17	-132	Chip	EAR99	HMC578
12.0 - 16.5	x2 Active	24 - 33	3	15	-132	LC3B	EAR99	HMC578LC3B
12.5 - 15.5	x2 Active	25 - 31	3	21	-	LP4	EAR99	HMC942LP4E
13.5 - 15.5	x2 Active	27 - 31	0	9	-132	LC3B	EAR99	HMC449LC3B
13.5 - 15.5	x2 Active	27 - 31	5	20	-128	LC4B	EAR99	HMC577LC4B
13.5 - 16.5	x2 Active	27 - 33	0	10	-132	Chip	EAR99	HMC449
16 - 23	x2 Active	32 - 46	3	13	-127	Chip	EAR99	HMC579
2.66 - 5.33	x3 Active	8 - 16	5	2	-152	LP3	EAR99	HMC916LP3E
1.5 - 2.5	x4 Active	6 - 10	5	2	-148	LP3	EAR99	HMC917LP3E
2.45 - 2.8	x4 Active	9.8 - 11.2	-15	3	-142	LP4	EAR99	HMC443LP4E
2.85 - 3.3	x4 Active	11.4 - 13.2	-15 to +5	7	-140	LP4	EAR99	HMC695LP4E
3.6 - 4.1	x4 Active	14.4 - 16.4	-15	0	-140	LP4	EAR99	HMC370LP4E
14 - 16	x4 Active	56 - 64	2	-6	-	Chip	3A001.b.2.f	HMC-XDH158
1.2375 - 1.4	x8 Active	9.9 - 11.2	-15	6	-136	LP4	EAR99	HMC444LP4E
0.61875 - 0.6875	x16 Active	9.9 - 11	-15	7	-130	LP4	EAR99	HMC445LP4E

#### FREQUENCY MULTIPLIERS - Passive

Input Frequency (GHz)	Function	Output Frequency (GHz)	Conversion Loss (dB)	1Fo / 4Fo Isolation (dB)	Input Drive (dBm)	Package	ECCN Code	Part Number
0.7 - 2.4	x2 Passive	1.4 - 4.8	15	47 / 38	10 to 20	Chip	EAR99	HMC156
0.7 - 2.4	x2 Passive	1.4 - 4.8	15	47 / 38	10 to 20	C8	EAR99	HMC156C8
0.85 - 2.0	x2 Passive	1.7 - 4.0	15	45 / 40	10 to 20	MS8	EAR99	HMC187AMS8E
1.25 - 3.0	x2 Passive	2.5 - 6.0	15	45 / 45	10 to 20	MS8	EAR99	HMC188MS8E
1.3 - 4.0	x2 Passive	2.6 - 8.0	15	45 / 40	10 to 20	Chip	EAR99	HMC158
1.3 - 4.0	x2 Passive	2.6 - 8.0	15	45 / 40	10 to 20	C8	EAR99	HMC158C8
2 - 4	x2 Passive	4 - 8	13	34 / 40	10 to 15	MS8	EAR99	HMC189AMS8E
4 - 8	x2 Passive	8 - 16	20	45 / 38	10 to 15	Chip	EAR99	HMC204
4 - 8	x2 Passive	8 - 16	17	41 / 40	10 to 15	C8	EAR99	HMC204C8
4 - 8	x2 Passive	8 - 16	17	42 / 50	10 to 15	MS8G	EAR99	HMC204MS8GE
6 - 12	x2 Passive	12 - 24	17	32 / 32	10 to 15	Chip	EAR99	HMC205
10 - 15	x2 Passive	20 - 30	13	30	+13	Chip	5A991.h	HMC-XDB112
12 - 18	x2 Passive	24 - 36	14	50 / 60	11 to 15	Chip	EAR99	HMC331
24 - 30	x3 Passive	72 - 90	19	-	+13	Chip	5A991.h	HMC-XTB110

#### PHASE LOCKED LOOP - Fractional-N & Integer-N ICs

Frequency	Function	Max. PFD Frequency	Max. Reference Frequency	Figure of Merit (Frac/Int) (dBc/Hz)	Frequency Resolution w/ 50 MHz Ref.	Bias Supply	Package	ECCN Code	Part Number
10 kHz - 8 GHz	Fractional-N with Sweeper	75 MHz	200 MHz	-221 / -227	3 Hz	+5V @ 37 mA +3.3V @ 90 mA	LP6C	3A001.a.11.b	HMC701LP6CE
10 kHz - 14 GHz	Fractional-N with Sweeper	75 MHz	200 MHz	-221 / -227	6 Hz	+5V @ 37 mA +3.3V @ 136 mA	LP6C	3A001.a.11.b	HMC702LP6CE
10 MHz - 8 GHz	Fractional-N	70 MHz	200 MHz	-221 / -226	3 Hz	+5V @ 7 mA +3.3V @ 95 mA	LP4	3A001.a.11.b	HMC700LP4E
DC - 7	Fractional-N with Sweeper	150 MHz	-	-228 / -231	10 Hz	+5V @ 97 mA +3V @ 149 mA	LP5	3A001.a.11.b	HMC983LP5E
DC - 7	Fractional-N with Sweeper	150 MHz	-	-228 / -231	10 Hz	+5V @ 97 mA +3V @ 149 mA	LP4	3A001.a.11.b	HMC984LP4E
DC - 8 GHz	Fractional-N with Sweeper	100 MHz	350 MHz	-230 / -233	3 Hz	+5V @ 6 mA +3.3V @ 52 mA	LP4	3A001.a.11.b	HMC703LP4E
DC - 8 GHz	Fractional-N	100 MHz	350 MHz	-230 / -233	3 Hz	+5V @ 6 mA +3.3V @ 52 mA	LP4	3A001.a.11.b	HMC704LP4E
80 MHz - 7 GHz	Integer-N	1300 MHz	1300 MHz	-233	50 MHz	+5V @ 310 mA	LP5	3A001.a.11.b	HMC698LP5E
160 MHz - 7 GHz	Integer-N	1300 MHz	1300 MHz	-233	50 MHz	+5V @ 310 mA	LP5	3A001.a.11.b	HMC699LP5E
10 MHz - 2.8 GHz	Integer-N	1300 MHz	1300 MHz	-233	50 MHz	+5V @ 250 mA	QS16G	3A001.a.11.b	HMC440QS16GE



## **SMT & Chip (Die) Products**

#### PLLs with INTEGRATED VCOs - Microwave & RF PLLs with Integrated VCOs

Frequency (MHz)	Function	Closed Loop SSB Phase Noise @ 10 kHz Offset	Open Loop VCO Phase Noise @ 1 MHz Offset	Pout (dBm)	RMS Jitter Fractional Mode (fs)	Integrated PN Fractional Mode (deg rms)	Package	ECCN Code	Part Number
io/2						(==g)			
665 - 825	Tri-Band RF VCO	-118 dBc/Hz	-148 dBc/Hz	11	180	0.05	LP6C	3A001.a.11.b	HMC822LP6CE
795 - 945	Tri-Band RF VCO	-123 dBc/Hz	-148 dBc/Hz	10	180	0.06	LP6C	3A001.a.11.b	HMC838LP6CE
780 - 870	RF VCO	-116 dBc/Hz	-148 dBc/Hz	14	180	0.06	LP6C	3A001.a.11.b	HMC824LP6CE
860 - 1040	Tri-Band RF VCO	-118 dBc/Hz	-147 dBc/Hz	10	180	0.07	LP6C	3A001.a.11.b	HMC821LP6CE
990 - 1105	RF VCO	-114 dBc/Hz	-146 dBc/Hz	11	180	0.07	LP6C	3A001.a.11.b	HMC826LP6CE
1025 - 1150	Tri-Band RF VCO	-123 dBc/Hz	-147 dBc/Hz	12	180	0.07	LP6C	3A001.a.11.b	HMC837LP6CE
1050 - 1205	Tri-Band RF VCO	-121 dBc/Hz	-146 dBc/Hz	10	180	0.08	LP6C	3A001.a.11.b	HMC839LP6CE
1095 - 1275	Tri-Band RF VCO	-118 dBc/Hz	-147 dBc/Hz	10	180	0.08	LP6C	3A001.a.11.b	HMC820LP6CI
1310 - 1415	Tri-Band RF VCO	-121 dBc/Hz	-145 dBc/Hz	10	180	0.09	LP6C	3A001.a.11.b	HMC840LP6CE
o									
1285 - 1415	RF VCO	-112 dBc/Hz	-143 dBc/Hz	10	180	0.09	LP6C	3A001.a.11.b	HMC828LP6CE
1330 - 1650	Tri-Band RF VCO	-112 dBc/Hz	-142 dBc/Hz	6.5	180	0.11	LP6C	3A001.a.11.b	HMC822LP6CE
1590 - 1890	Tri-Band RF VCO	-118 dBc/Hz	-143 dBc/Hz	7.5	180	0.12	LP6C	3A001.a.11.b	HMC838LP6CE
1720 - 2080	Tri-Band RF VCO	-112 dBc/Hz	-141 dBc/Hz	6.5	180	0.13	LP6C	3A001.a.11.b	HMC821LP6CE
1815 - 2010	RF VCO	-112 dBc/Hz	-143 dBc/Hz	7.5	180	0.13	LP6C	3A001.a.11.b	HMC831LP6CE
2050 - 2300	Tri-Band RF VCO	-117 dBc/Hz	-141 dBc/Hz	10.5	180	0.15	LP6C	3A001.a.11.b	HMC837LP6CE
2100 - 2410	Tri-Band RF VCO	-115 dBc/Hz	-140 dBc/Hz	7.5	180	0.16	LP6C	3A001.a.11.b	HMC839LP6CI
2190 - 2550	Tri-Band RF VCO	-112 dBc/Hz	-141 dBc/Hz	6.5	180	0.17	LP6C	3A001.a.11.b	HMC820LP6CI
2620 - 2830	Tri-Band RF VCO	-115 dBc/Hz	-139 dBc/Hz	9	180	0.18	LP6C	3A001.a.11.b	HMC840LP6C
2fo	III Balla III VOO	110 000/112	100 000/112	-	100	0.10	LI 00	0/1001.4.11.5	THINGO TO LET GOT
2660 - 3300	Tri-Band RF VCO	-106 dBc/Hz	-136 dBc/Hz	-4	180	0.21	LP6C	3A001.a.11.b	HMC822LP6CE
3180 - 3780	Tri-Band RF VCO	-112 dBc/Hz	-135 dBc/Hz	-4	180	0.24	LP6C	3A001.a.11.b	HMC838LP6CE
3365 - 3705	RF VCO	-107 dBc/Hz	-135 dBc/Hz	0	190	0.25	LP6C	3A001.a.11.b	HMC836LP6CE
3440 - 4160	Tri-Band RF VCO	-107 dBc/Hz	-135 dBc/Hz	-4	180	0.27	LP6C	3A001.a.11.b	HMC821LP6CE
4100 - 4600	Tri-Band RF VCO	-111 dBc/Hz	-135 dBc/Hz	-0.5	180	0.30	LP6C	3A001.a.11.b	HMC837LP6CE
4200 - 4820	Tri-Band RF VCO	-108 dBc/Hz	-135 dBc/Hz	-4	180	0.31	LP6C	3A001.a.11.b	HMC839LP6CE
4380 - 5100	Tri-Band RF VCO	-106 dBc/Hz	-135 dBc/Hz	-4	180	0.33	LP6C	3A001.a.11.b	HMC820LP6CE
5240 - 5660	Tri-Band RF VCO	-100 dBc/Hz	-133 dBc/Hz	-3	180	0.37	LP6C	3A001.a.11.b	HMC840LP6CE
7300 - 8200	Microwave PLL+VCO	-109 dBc/Hz	-140 dBc/Hz	15	196	0.58	LP6C	3A001.a.11.b	HMC764LP6CE
7800 - 8800	Microwave PLL+VCO	-101 dBc/Hz	-140 dBc/Hz	13	193	0.61	LP6C	3A001.a.11.b	HMC765LP6CE
8450 - 9550	Microwave PLL+VCO	-107 dBc/Hz	-138 dBc/Hz	12	93	0.30	LP6C	3A001.a.11.b	HMC767LP6CE
9050 - 10150	Microwave PLL+VCO	-107 dBc/Hz	-140 dBc/Hz	12	82	0.28	LP6C	3A001.a.11.b	HMC769LP6CE
9600 - 10800	Microwave PLL+VCO	-106 dBc/Hz	-140 dBc/Hz	9	83	0.31	LP6C	3A001.a.11.b	HMC778LP6CE
11500 - 12500	Microwave PLL+VCO	-99 dBc/Hz	-134 dBc/Hz	10	181	0.81	LP6C	3A001.a.11.b	HMC783LP6CI
12400 - 13400	Microwave PLL+VCO	-98 dBc/Hz	-134 dBc/Hz	8	175	0.84	LP6C	3A001.a.11.b	HMC807LP6CE
	ntinuous Tuning	-90 UDC/112	-132 UDC/112	- 0	173	0.04	LFOC	3A001.a.11.b	TIWIC 807 EF 0CI
25 - 3000	Wideband RF VCO	-114 dBc/Hz @ 2 GHz	-141 dBc/Hz @ 2 GHz	5	82 [1]	0.114 @ 2 GHz	LP6G	3A001.a.11.b	HMC830LP6GI
25 - 6000	Wideband RF VCO	-114 dBc/Hz @ 2 GHz	-135 dBc/Hz @ 4 GHz	-4	82 [1]	0.22 @ 4 GHz	LP6G	3A001.a.11.b	HMC833LP6GE
45 - 1050 1400 - 2100 2800 - 4200 Fo	Wideband RF VCO	-108 dBc/Hz @ 4 GHz	-134 dBc/Hz @ 4 GHz	4	82 [1]	0.229 @ 4 GHz	LP6G	3A001.a.11.b	HMC829LP6GE
45 - 1050 1400 - 2100 2800 - 4200 Fo 5600 - 8400	Wideband RF VCO	-108 dBc/Hz @ 4 GHz	-128 dBc/Hz @ 8 GHz	5 2 2 -10	82 [1]	0.46 @ 8 GHz	LP6G	3A001.a.11.b	HMC834LP6GE

<sup>[1]</sup> RMS Jitter Integration Bandwidth from 12 kHz to 20 MHz

### VOLTAGE CONTROLLED OSCILLATORS\* - VCOs with Buffer Amplifiers & Wideband VCOs

Fo Frequency (GHz)	Function	Fo Output Power (dBm)	10 kHz SSB Phase Noise (dBc/Hz)	100 kHz SSB Phase Noise (dBc/Hz)	Bias Supply	Package	ECCN Code	Part Number
2.05 - 2.25	VCO with Buffer	3.5	-89	-112	+3V @ 35 mA	LP4	EAR99	HMC384LP4E
2.25 - 2.5	VCO with Buffer	4.5	-89	-115	+3V @ 35 mA	LP4	EAR99	HMC385LP4E
2.6 - 2.8	VCO with Buffer	5	-88	-115	+3V @ 35 mA	LP4	EAR99	HMC386LP4E
2.75 - 3.0	VCO with Buffer	4.5	-89	-114	+3V @ 37 mA	LP4	EAR99	HMC416LP4E
3.15 - 3.4	VCO with Buffer	4.9	-88	-113	+3V @ 39 mA	LP4	EAR99	HMC388LP4E
3.35 - 3.55	VCO with Buffer	4.7	-89	-112	+3V @ 41 mA	LP4	EAR99	HMC389LP4E
3.55 - 3.9	VCO with Buffer	4.7	-87	-112	+3V @ 42 mA	LP4	EAR99	HMC390LP4E
3.9 - 4.45	VCO with Buffer	5	-81	-106	+3V @ 30 mA	LP4	EAR99	HMC391LP4E
4.45 - 5.0	VCO with Buffer	4	-79	-105	+3V @ 30 mA	LP4	EAR99	HMC429LP4E
5.0 - 5.5	VCO with Buffer	2	-80	-103	+3V @ 27 mA	LP4	EAR99	HMC430LP4E
5.5 - 6.1	VCO with Buffer	2	-80	-102	+3V @ 27 mA	LP4	EAR99	HMC431LP4E
5.8 - 6.8	VCO with Buffer	10	-82	-105	+3V @ 100 mA	MS8G	EAR99	HMC358MS8GE
6.1 - 6.72	VCO with Buffer	4.5	-73	-101	+3V @ 31 mA	LP4	EAR99	HMC466LP4E



### SMT & Chip (Die) Products

#### VOLTAGE CONTROLLED OSCILLATORS\* - VCOs with Buffer Amplifiers & Wideband VCOs

Fo Frequency (GHz)	Function	Fo Output Power (dBm)	10 kHz SSB Phase Noise (dBc/Hz)	100 kHz SSB Phase Noise (dBc/Hz)	Bias Supply	Package	ECCN Code	Part Number
6.8 - 7.4	VCO with Buffer	11	-80	-106	+3V @ 80 mA	LP4	EAR99	HMC505LP4E
7.1 - 7.9	VCO with Buffer	14	-80	-101	+3V @ 85 mA	LP4	EAR99	HMC532LP4E
7.8 - 8.7	VCO with Buffer	14	-80	-103	+3V @ 77 mA	LP4	EAR99	HMC506LP4E
8.6 - 10.2	VCO with ÷4	18	-70	-100	+5V @ 220 mA	LP5	3A001.a.11.b	HMC734LP5E
10.5 - 12.2	VCO with ÷4	17	-75	-100	+5V @ 220 mA	LP5	3A001.a.11.b	HMC735LP5E
13.2 -13.5	VCO with ÷8	-8	-83	-110	+5V @ 230 mA	QS16G	3A001.a.11.b	HMC401QS16GE
14.0 - 15.0	VCO with ÷8	6	-75	-110	+5V @ 260 mA	QS16G	3A001.a.11.b	HMC398QS16GE
23.8 - 24.8	VCO with ÷16	12	-70	-95	+5V @ 220 mA	LP4	3A001.a.11.b	HMC533LP4E
4 - 8	Wideband VCO	5	-75	-100	+5V @ 55 mA	LC4B	EAR99	HMC586LC4B
5 - 10	Wideband VCO	5	-65	-95	+5V @ 55 mA	LC4B	EAR99	HMC587LC4B
6 - 12	Wideband VCO	1	-65	-95	+5V @ 57 mA	LC4B	EAR99	HMC732LC4B
8 - 12.5	Wideband VCO	5	-65	-93	+5V @ 55 mA	LC4B	EAR99	HMC588LC4B
10 - 20	Wideband VCO	3	-60	-90	+5V @ 70 mA	LC4B	EAR99	HMC733LC4B

<sup>\*</sup> HMC VCOs integrate resonator, negative resistance generator and tuning varactor circuits on-chip. No external components are required.

#### VOLTAGE CONTROLLED OSCILLATORS WITH Fo/2 OLITPLIT

Fo Frequency (GHz)	Fo/2 Frequency (GHz)	Function	Fo Output Power (dBm)	10 kHz SSB Phase Noise (dBc/Hz)	100 kHz SSB Phase Noise (dBc/Hz)	Bias Supply	Package	ECCN Code	Part Number
VCOs with Fo/2	2								
6.65 - 7.65	3.325 - 3.825	VCO with Fo/2	13	-90	-115	+5V @ 230 mA	LP5	EAR99	HMC507LP5E
7.3 - 8.2	3.65 - 4.1	VCO with Fo/2	15	-90	-116	+5V @ 240 mA	LP5	EAR99	HMC508LP5E
7.8 - 8.8	3.9 - 4.4	VCO with Fo/2	13	-90	-115	+5V @ 250 mA	LP5	EAR99	HMC509LP5E
9.05 - 10.15	4.525 - 5.075	VCO with Fo/2	13	-88	-115	+5V @ 265 mA	LP5	EAR99	HMC511LP5E
14.5 - 15.0	7.25 - 7.5	VCO with Fo/2	9	-80	-105	+4.2V @ 150 mA	LP4	EAR99	HMC736LP4E
14.9 - 15.5	7.45 - 7.75	VCO with Fo/2	9	-80	-105	+4.2V @ 150 mA	LP4	EAR99	HMC737LP4E
VCOs with Fo/2	2 & ÷4								
8.45 - 9.55	4.225 - 4.775	VCO with Fo/2 & ÷4	13	-92	-116	+5V @ 315 mA	LP5	3A001.a.11.b	HMC510LP5E
9.5 - 10.8	4.75 - 5.4	VCO with Fo/2 & ÷4	11	-85	-110	+5V @ 350 mA	LP5	3A001.a.11.b	HMC530LP5E
9.6 - 10.8	4.8 - 5.4	VCO with Fo/2 & ÷4	9	-85	-111	+5V @ 330 mA	LP5	3A001.a.11.b	HMC512LP5E
10.43 - 11.46	5.215 - 5.73	VCO with Fo/2 & ÷4	7	-85	-110	+3V @ 275 mA	LP5	3A001.a.11.b	HMC513LP5E
10.6 - 11.8	5.3 - 5.9	VCO with Fo/2 & ÷4	11	-82	-110	+5V @ 350 mA	LP5	3A001.a.11.b	HMC534LP5E
11.1 - 12.4	5.55 - 6.2	VCO with Fo/2 & ÷4	9	-83	-110	+5V @ 350 mA	LP5	3A001.a.11.b	HMC582LP5E
11.17 - 12.02	5.585 - 6.01	VCO with Fo/2 & ÷4	7	-87	-110	+3V @ 275 mA	LP5	3A001.a.11.b	HMC514LP5E
11.5 - 12.5	5.75 - 6.25	VCO with Fo/2 & ÷4	10	-83	-110	+5V @ 200 mA	LP5	3A001.a.11.b	HMC515LP5E
11.5 - 12.8	5.75 - 6.4	VCO with Fo/2 & ÷4	11	-80	-110	+5V @ 350 mA	LP5	3A001.a.11.b	HMC583LP5E
12.4 - 13.4	6.2 - 6.7	VCO with Fo/2 & ÷4	8	-83	-110	+5V @ 260 mA	LP5	3A001.a.11.b	HMC529LP5E
12.5 - 13.9	6.25 - 6.95	VCO with Fo/2 & ÷4	10	-81	-110	+5V @ 330 mA	LP5	3A001.a.11.b	HMC584LP5E
13.6 - 14.9	6.8 - 7.45	VCO with Fo/2 & ÷4	7	-82	-110	+5V @ 260 mA	LP5	3A001.a.11.b	HMC531LP5E
14.25 - 15.65	7.125 - 7.825	VCO with Fo/2 & ÷4	9	-80	-107	+5V @ 350 mA	LP5	3A001.a.11.b	HMC632LP5E
VCOs with Fo/2	2 & ÷16								
20.9 - 23.9	10.45 - 11.95	VCO with Fo/2 & ÷16	9	-65	-95	+5V @ 200 mA	LP4	3A001.a.11.b	HMC738LP4E
23.8 - 26.8	11.9 - 13.4	VCO with Fo/2 & ÷16	8	-64	-93	+5V @ 200 mA	LP4	3A001.a.11.b	HMC739LP4E

#### PHASE LOCKED OSCILLATOR

TIAGE LOC	THASE ECORED OSCILLATOR													
Fo Frequency (GHz)	Function	Fo Output Power (dBm)		100 kHz SSB Phase Noise (dBc/Hz)	Bias Supply	Package	ECCN Code	Part Number						
14.7 - 15.4	Phase Locked Oscillator	9	-80	-110	+5V @ 340 mA +12V @ 28 mA	LP4	3A001.a.11.b	HMC535LP4E						

## Market & Application Guide



#### for LO Generation Applications

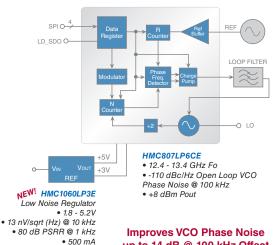
#### HITTITE'S HIGH FREQUENCY LO SOURCE ALTERNATIVES

#### PLL & VCO CHIPSET

#### HMC702LP6CE Fractional-N PLL • 10 KHz to 14 GHz • -227 FOM Integer Mode Sigma HMC584LP5E VCO with Fo/2 & Fo/4 Output +5V • 12.5 - 13.9 GHz Fo Low Phase Noise -110 dBc/Hz @ 100 kHz • +10 dBm Pout HMC860LP3E High PSRR DC Regulator 2.5V - 5.2V • 80 dB PSRR @ 1 MHz HMC9761 P3F • 240 mA High PSRR DC Regulator • 1.8V - 5.1V • 60 dB PSSR @ 1 kHz • 400 mA **Improves VCO Phase Noise** up to 14 dB @ 100 kHz Offset

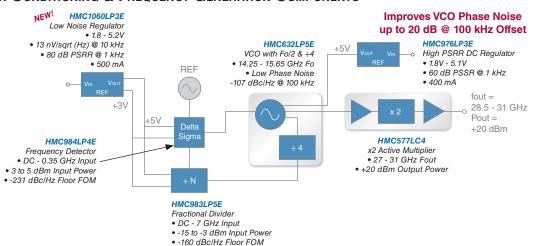
Contact Us: PLL@hittite.com

#### PLL WITH INTEGRATED VCO IC

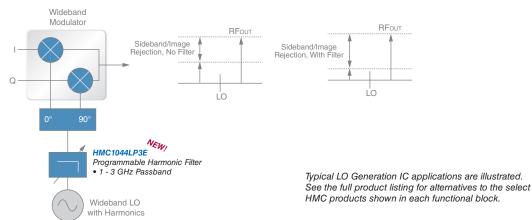


Improves VCO Phase Noise up to 14 dB @ 100 kHz Offset

#### KA BAND PHASE LOCKED OSCILLATOR FEATURING HITTITE'S DC Power Conditioning & Frequency Generation Components



### Using HMC1044LP3E as an LO Harmonic Filter to IMPROVE MODULATOR/DEMODULATOR SIDEBAND/IMAGE REJECTION

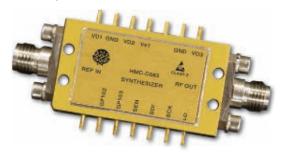


MAY 2012



#### **Robust, High Performance RF to Light Solutions**

Our hermetic module product line spans a wide range of popular product types including amplifiers, attenuators, DROs, high speed digital logic, frequency multipliers, MicroSynth® integrated synthesizers, mixers, phase shifters, prescalers, SDLVAs, switches & VCOs. Utilizing our standard MMIC products, we take advantage of our world-class design, manufacturing and quality expertise. Hittite can also upscreen modules for high-reliability/military specification applications. Contact us to discuss your custom module requirements.



#### Features:

- ♦ Off-The-Shelf Availability
- ♦ Hermetically Sealed
- ♦ Internal DC Power Regulation
- ♦ Field Replaceable Connectors
- ♦ Military & Space Upscreening
- ♦ Customization Offered

#### **AMPLIFIERS**

Frequency (GHz)	Function	Gain (dB)	OIP3 (dBm)	NF (dB)	P1dB (dBm)	Bias Supply	Package / Connector	ECCN Code	Part Number
1 - 12	Low Noise	16	30	1.8	16	+6V @ 60 mA	C-10B / SMA	EAR99	HMC-C059
1.8 - 4.2	Low Noise	26	26	0.7	15.5	+8V @ 112 mA	C-10 / SMA	EAR99	HMC-C04
5 - 9	Low Noise	22.5	25	1.75	15	+12V @ 105 mA	C-10 / SMA	EAR99	HMC-C04
29 - 36	Low Noise	20	22	2.9	11	+3V @ 80 mA	C-10 / 2.92 mm	3A001.b.4.c	HMC-C02
2 - 20	Wideband LNA	15	25	2.5	14	+12V @ 65 mA	C-1 / SMA	EAR99	HMC-C00
2 - 20	Wideband LNA	14	26	2	18	+12V @ 60 mA	C-2 / SMA	EAR99	HMC-C00
2 - 20	Wideband LNA	14	27	2	16	+8V @ 75 mA	C-2B / SMA	EAR99	HMC-C02
7 - 17	Wideband LNA	22	25	2	14	+8V @ 93 mA	C-1 / SMA	EAR99	HMC-C01
17 - 27	Wideband LNA	18	25	3	14	+8V @ 96 mA	C-1B / 2.92 mm	EAR99	HMC-C01
0.01 - 20	Wideband Driver	16	33	3	23	+12V @ 195 mA	C-3 / SMA	3A001.b.4.f	HMC-C00
0.01 - 20	Wideband Driver	15	30	3	23	+12V @ 225 mA	C-3B / SMA	3A001.b.4.f	HMC-C02
2 - 35	Wideband Driver	12	29	3	18	+11V @ 92 mA	C-10 / 2.92 mm	3A001.b.4.c	HMC-C03
0.01 - 6.0	Single Stage Power Amplifier, 1 Watt	13	40	5	29.5	-5V @ 5 mA +15V @ 450 mA	C-17 / SMA	EAR99	HMC-C07
0.01 - 6.0	Two Stage Power Amplifier, 1 Watt	24	42	5	29.5	-5V @ 5 mA +15V @ 740 mA	C-17 / SMA	EAR99	HMC-C07
0.01 - 15	Wideband Power Amplifier, 1/2 Watt	12	36	4	28	+11V @ 360 mA	C-10B / SMA	3A001.b.4.f	HMC-C03
0.01 - 15	Wideband Power Amplifier, 1/2 Watt	12	36	4	28	+11V @ 360 mA	C-12 / SMA	3A001.b.4.f	HMC-C03
2 - 20	Wideband Power Amplifier	15	34	4	26	+12V @ 310 mA	C-2 / SMA	3A001.b.4.f	HMC-C00
2 - 20	Wideband Power Amplifier	15	34	4	26	+12V @ 310 mA	C-2B / SMA	3A001.b.4.f	HMC-C02
2 - 20	Wideband Power Amplifier	31	33	3	26	+12V @ 400 mA	C-3B / SMA	3A001.b.4.f	HMC-C02
17 - 24	Wideband Power Amplifier	22	33	3.5	24	+8V @ 250 mA	C-10 / 2.92 mm	EAR99	HMC-C02
21 - 31	Wideband Power Amplifier	15	32	5	24	+8V @ 215 mA	C-10 / 2.92 mm	3A001.b.4.c	HMC-C02
0.8 - 2.0	Power Amplifier, 10 Watt	43	56	12	40	+12V @ 6.5A	C-7 / SMA	EAR99	HMC-C01

#### **AMPLIFIERS - Low Phase Noise**

Frequency (GHz)	Function	Gain / NF (dB)	OIP3 (dBm)	10 kHz Phase Noise (dBc/Hz)	P1dB / Psat (dBm)	Bias Supply	Package / Connector	ECCN Code	Part Number
1.5 - 5.0	Low Phase Noise	14 / 4.5	26.5	-171	17 / 22	+7V @ 170 mA	C-16 / SMA	EAR99	HMC-C077
2 - 18	Low Phase Noise	13.5 / 5	22.5	-160	15 / 18.5	+5V @ 80 mA	C-1 / SMA	EAR99	HMC-C050
3 - 8	Low Phase Noise	9/6	33	-168	22 / 25	+7V @ 300 mA	C-16 / SMA	EAR99	HMC-C079
6 - 12	Low Phase Noise	11 / 4.5	34	-176	20 / 22	+7V @ 170 mA	C-16 / SMA	EAR99	HMC-C072
7 - 11	Low Phase Noise	9/6	33	-170	22 / 25	+7V @ 300 mA	C-16 / SMA	EAR99	HMC-C076

#### **ATTENUATORS** - Analog & Digital

Frequency (GHz)	Function	Loss (dB)	Attenuation Range (dB)	IIP3 (dBm)	Control Input (Vdc)	Package / Connector	ECCN Code	Part Number
DC - 20	Analog VVA	5.5	35	10	-5	C-10 / SMA	EAR99	HMC-C053
DC - 13	6-Bit Digital, Serial Control	3.6	0.5 to 31.5	32	Serial/CMOS	C-6 / SMA	EAR99	HMC-C018
DC - 13	6-Bit Digital	3.2	0.5 to 31.5	38	0 / +5V	C-6 / SMA	EAR99	HMC-C025

#### **DIELECTRIC RESONATOR OSCILLATORS (DRO)**

Frequency (GHz)	Function	Output Power (dBm)	Phase Noise	100 kHz SSB Phase Noise (dBc/Hz)		Bias Supply	Package	ECCN Code	Part Number
8.0 - 8.3	Dielectric Resonator Oscillator	14.5	-122	-140	2	+6 to +15V @ 125 mA	C-18 / SMA	EAR99	HMC-C200



### **Robust, High Performance RF to Light Solutions**

#### FREQUENCY DIVIDERS (PRESCALERS)

Input Freq. (GHz)	Function	Input Power (dBm)	Output Power (dBm)	100 kHz SSB Phase Noise (dBc/Hz)	Bias Supply	Package / Connector	ECCN Code	Part Number
DC - 18	Divide-by-2	-15 to +10	-4	-150	+5V @ 75 mA	C-1 / SMA	3A001.a.11.b	HMC-C005
DC - 18	Divide-by-4	-15 to +10	-4	-150	+5V @ 93 mA	C-1 / SMA	3A001.a.11.b	HMC-C006
0.5 - 8	Divide-by-5	-15 to +10	-1	-155	+5V @ 80 mA	C-1 / SMA	3A001.a.11.b	HMC-C039
DC - 18	Divide-by-8	-15 to +10	-4	-150	+5V @ 98 mA	C-1 / SMA	3A001.a.11.b	HMC-C007
0.5 - 17	Divide-by-10	-15 to +10	-1	-155	+5V @ 152 mA	C-1 / SMA	3A001.a.11.b	HMC-C040

#### FREQUENCY MULTIPLIERS - Active

Input Freq. (GHz)	Function	Output Freq. (GHz)	Input Power (dBm)	Output Power (dBm)	100 kHz SSB Phase Noise (dBc/Hz)	Package / Connector	ECCN Code	Part Number
3 - 5	x2 Active	6 - 10	3	17	-140	C-10 / SMA	EAR99	HMC-C031
9.0 - 14.5	x2 Active	18 - 29	3	16	-132	C-10 / 2.92 mm	EAR99	HMC-C032
12.0 - 16.5	x2 Active	24 - 33	3	17	-132	C-10 / 2.92 mm	EAR99	HMC-C033
16 - 23	x2 Active	32 - 46	3	13	-130	C-10 / 2.92 mm	EAR99	HMC-C034
4.0 - 10.5	x2 Active	8 - 21	6	14	-142	C-10 / SMA	EAR99	HMC-C056

#### HIGH SPEED DIGITAL LOGIC

Data / Clock Rate (Gbps / GHz)	Function	Rise / Fall Time (ps)	Deterministic Jitter (ps)	Differential Output Swing (Vp-p)	DC Power (mW)	Vee Power Supply (Vdc)	Package / Connector	ECCN Code	Part Number
50 / 30	1:2 Fanout Buffer	9.5 / 11	2	0.5	455	-3.3	C-13 / 1.85 mm	3A001.a.11.b	HMC-C062
50 / 25	AND / NAND / OR / NOR	9 / 10	2	0.5	560	-3.3	C-13 / 1.85 mm	3A001.a.11.b	HMC-C065
43 / 43	D-Type Flip-Flop	9 / 10	1.5	0.5	580	-3.3	C-13 / 1.85 mm	3A001.a.11.b	HMC-C060
50 / 25	D-Type Flip-Flop Double Edge Triggered	9 / 11	1.5	0.5	690	-3.3	C-13 / 1.85 mm	3A001.a.11.b	HMC-C061
50 / 25	XOR / XNOR	6.5 / 10	2	0.5	550	-3.3	C-13 / 1.85 mm	3A001.a.11.b	HMC-C064

#### **I/Q MIXERS**

RF / LO Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	Image Rejection (dB)	IIP3 (dBm)	Package / Connector	ECCN Code	Part Number
4 - 8.5	I/Q Mixer / IRM	DC - 3.5	-7.5	35	23	C-4 / SMA	EAR99	HMC-C009
6 - 10	I/Q Mixer / IRM	DC - 3.5	-7.5	35	25	C-4 / SMA	EAR99	HMC-C041
8.5 - 13.5	I/Q Mixer / IRM	DC - 2	-8	28	25	C-4 / SMA	EAR99	HMC-C042
11 - 16	I/Q Mixer / IRM	DC - 3.5	-9	30	28	C-4 / SMA	EAR99	HMC-C043
15 - 23	I/Q Mixer / IRM	DC - 3.5	-8	30	25	C-4 / 2.92 mm & SMA	EAR99	HMC-C044
20 - 31	I/Q Mixer / IRM	DC - 4.5	-10	24	22.5	C-4B / 2.92 mm & SMA	EAR99	HMC-C046
30 - 38	I/Q Mixer / IRM	DC - 3.5	-10.5	15	19	C-4 / 2.92 mm & SMA	EAR99	HMC-C047

#### **MIXERS**

RF Frequency (GHz)	Function	IF Frequency (GHz)	Conversion Gain (dB)	LO/RF Isolation (dB)	IIP3 (dBm)	Package / Connector	ECCN Code	Part Number
7 - 14	+13 LO, DBL-BAL	DC - 5	-7	48	20	C-11 / SMA	EAR99	HMC-C049
11 - 20	+13 LO, DBL-BAL	DC - 6	-7	43	18	C-11 / 2.92 mm & SMA	EAR99	HMC-C051
16 - 32	+13 LO, DBL-BAL	DC - 8	-8	35	19	C-11 / 2.92 mm & SMA	EAR99	HMC-C014
23 - 37	+13 LO, DBL-BAL	DC - 13	-9	35	19	C-11 / 2.92 mm & SMA	EAR99	HMC-C035
24 - 38	+13 LO, DBL-BAL	DC - 8	-8.5	35	20	C-11 / 2.92 mm & SMA	EAR99	HMC-C015

#### PHASE SHIFTERS - Analog

Frequency (GHz)	Function	Insertion Loss (dB)	Phase Range (deg)	2nd harmonic Pin = 10 dBm (dBc)	Control Voltage Range (Vdc)	Package / Connector	ECCN Code	Part Number
6 - 15	Analog	7	750° @ 6 GHz 450° @ 15 GHz	40	0V to +5V	C-1 / SMA	EAR99	HMC-C010

#### PHASE SHIFTERS - Digital

Frequency	Function	Insertion	Phase	IIP3	Control Voltage	Package /	ECCN	Part
(GHz)		Loss (dB)	Range (deg)	(dBm)	Range (Vdc)	Connector	Code	Number
8 - 12	4-Bit Digital	7	22.5 to 360	38	0V to +5V	C-6 / SMA	EAR99	HMC-C055

### SDLVAs - Successive Detection Log Video Amplifier

Frequency (GHz)	Function	Dynamic Range (dB)	RSSI Slope (mV / dB)	RF Threshold Level (dBm)	Bias Supply	Package / Connector	ECCN Code	Part Number
1 - 20	SDLVA	59	14	-67	+12V @ 86 mA	C-10 / 2.92 mm	EAR99	HMC-C052
2 - 20	SDLVA with Limited RF Output	50	45	-45	+12V @ 370 mA -5V @ 20 mA	C-21 / SMA	EAR99	HMC-C078



## Robust, High Performance RF to Light Solutions

#### SWITCHES - SPST, SPDT & SP4T

Frequency (GHz)	Function	Insertion Loss (dB)	Isolation (dB)	Input P1dB (dBm)	Switching Speed (ns)	Package / Connector	ECCN Code	Part Number
DC - 20	SPST, Hi Isolation	3	100	23	8.5	C-9 / SMA	EAR99	HMC-C019
DC - 18	SPDT, Hi Isolation	2	55	27	3	C-14 / SMA	EAR99	HMC-C058
DC - 20	SPDT, Hi Isolation	2	40	23	5	C-5 / SMA	EAR99	HMC-C011
DC - 20	SP4T, Hi Isolation	3	40	24	14	C-15 / SMA	EAR99	HMC-C071

#### SYNTHESIZED MODULES - MicroSynth®

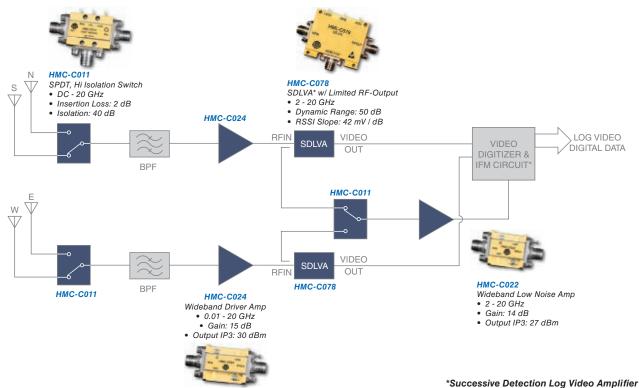
Frequency (GHz)	Function	Min. Step Size Resolution (Hz)	Reference Frequency (MHz)	SSB Phase Noise @ 100 kHz Offset (dBc/Hz)	Output Power (dBm)	Bias Supply	Package	ECCN Code	Part Number
2 - 6	MicroSynth® Synthesizer	0.6	10	-93	17	+20V @ 7 mA +6V @ 330 mA	C-20 / SMA	EAR99	HMC-C083
5.5 - 10.5	MicroSynth® Synthesizer	1.2	10	-92	21	+20V @ 20 mA +6V @ 300 mA +3.6V @ 100 mA	C-20 / SMA	EAR99	HMC-C070

#### **VOLTAGE CONTROLLED OSCILLATORS**

Frequency (GHz)	Function	Output Power (dBm)	10 kHz SSB Phase Noise (dBc/Hz)	100 kHz SSB Phase Noise (dBc/Hz)	Bias Supply	Package / Connector	ECCN Code	Part Number
4 - 8	Wideband VCO	20	-75	-95	+12V @ 185 mA	C-1 / SMA	EAR99	HMC-C028
5 - 10	Wideband VCO	20	-64	-93	+12V @ 195 mA	C-1 / SMA	EAR99	HMC-C029
8 - 12.5	Wideband VCO	21	-59	-83	+12V @ 195 mA	C-1 / SMA	EAR99	HMC-C030
38.4 - 43.2	VCO	13	-74	-98	+5V @ 350 mA	C-19 / 2.4 mm	EAR99	HMC-C073

Hittite Microwave Can Offer Any Of Our Die Or SMT IC Products In A Connectorized Module. Full Specifications for Each Product Are Available at www.hittite.com.

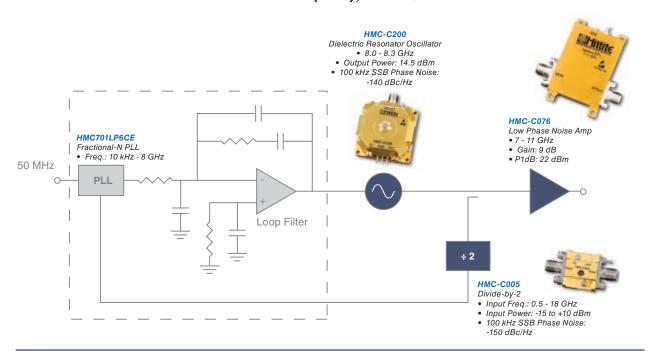
#### MILITARY RADAR RECEIVER SOLUTION



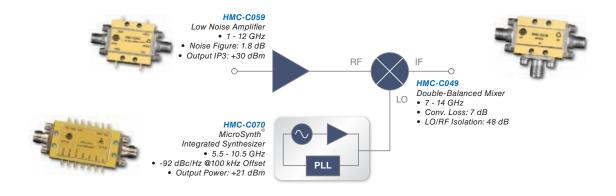


#### **Robust, High Performance RF to Light Solutions**

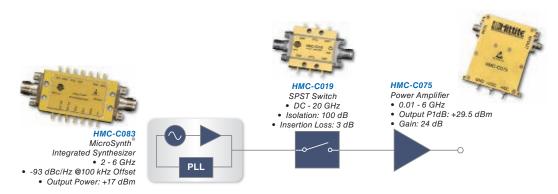
#### ULTRA LOW NOISE PHASE LOCKED OSCILLATOR (PLO), TEST EQUIPMENT SOLUTION



#### X-BAND MILTARY DOWNCONVERTER SOLUTION



#### Pulsed 0.5W C-BAND MILTARY & TEST EQUIPMENT SYNTHESIZER SOLUTION







### **Expanded Signal Generator Family to 70 GHz**







10 MHz to 20 GHz



## **Our Signal Generator Products**

- ♦ Wide Frequency Range: 10 MHz to 70 GHz
- ♦ Versatile: High Output Power Simplifies Test Set-Ups
- ♦ Efficient: Fast Frequency Switching Below 500 µs
- ♦ Flexible: Manual or USB / GPIB / Ethernet Control



10 MHz to 20 GHz

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# 10 MHz to 40 GHz



- ♦ High Output Power: +20 dBm @ 40 GHz
- ♦ Excellent 10 GHz SSB Phase Noise: -98 dBc/Hz @ 10 kHz Offset
- ♦ Spurious: < -65 dBc @ 10 GHz
- ♦ Resolution: 0.1 dB & 1 Hz
- ♦ Fast Switching: 500 µs

# 10 MHz to 70 GHz



- ♦ Output Power: +3dBm @ 70 GHz
- ♦ Excellent 70 GHz SSB Phase Noise: -79 dBc/Hz @ 10 kHz Offset
- ♦ Spurious: < -65 dBc @ 10 GHz
- ♦ Resolution: 0.1 dB & 1 Hz
- ♦ Fast Switching: 500 µs

## **INSTRUMENTATION**

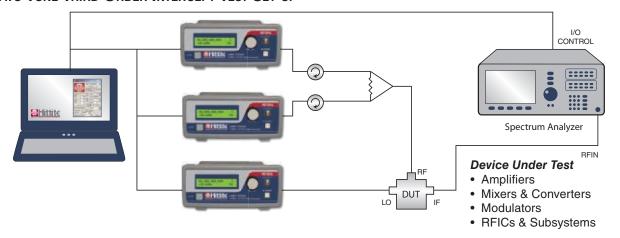


### **Expanded Signal Generator Family to 40 GHz**

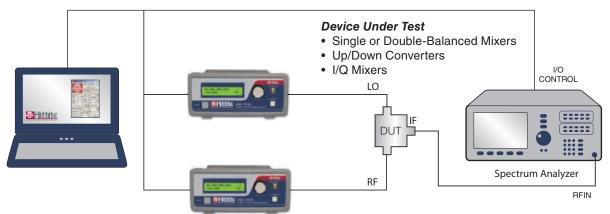
#### SIGNAL GENERATORS - Precise RF Signal Generation for ATE & Lab Environments

Frequency (GHz)	Function	Frequency Resolution	Maximum Power Output (dBm)	100 kHz SSB Phase Noise (dBc/Hz)	Spurious (dBc)	Switching Speed Steps (µs)	Package	ECCN Code	Part Number
0.7 - 8.0	Signal Generator	1 MHz	+17 @ 1 GHz +10 @ 8 GHz	-87 @ 4 GHz	< -45	200	Rack Mountable / Benchtop	EAR99	HMC-T2000
0.01 - 20	Signal Generator	10 kHz	+25 @ 1 GHz +22 @ 20 GHz	-93 @ 10 GHz	< -27	300	Rack Mountable / Benchtop	EAR99	HMC-T2100
0.01 - 20	Portable Signal Generator	1 Hz	+28 @ 1 GHz +24 @ 20 GHz	-99 @ 10 GHz	< -57	300	Portable / Benchtop	EAR99	HMC-T2220B
0.01 - 20	Signal Generator	1 Hz	+28 @ 1 GHz +24 @ 20 GHz	-99 @ 10 GHz	< -57	300	Rack Mountable / Benchtop	EAR99	HMC-T2220
0.01 - 40	Signal Generator	1 Hz	+30 @ 1 GHz +20 @ 40 GHz	-99 @ 10 GHz	< -52	500	Rack Mountable / Benchtop	EAR99	HMC-T2240
0.01 - 70	Signal Generator	1 Hz	+29 @ 1 GHz +3 @ 70 GHz	-118 @ 1 GHz -79 @ 70 GHz	< -46	500	Rackmountable / Benchtop	3A002.d.3.f	HMC-T2270

#### Two Tone Third Order Intercept Test Set-up



#### EFFICIENT MIXER CONVERSION LOSS, ISOLATION & MXN SPURIOUS TEST SET-UP



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- Design, production & screening of highly integrated MIC sub-assemblies for major defense OEMs.
- Military & Space Upscreening to Customer Specifications.

#### Military Solution Inquiries: MIL@hittite.com





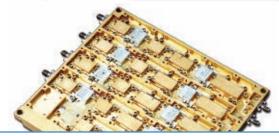




#### **Class B Screening & Qualification**

- VI to Method 2010B & 2017H
- Bond Pull & Die Shear Test
- Solderability Test
- High Temp Burn-In Test
- Vibration Stress Test
- Temp Cycle Stress Test
- Constant Acceleration Stress Test
- Fine & Gross Hermeticity Test
- Serialized Test Data
- ESD Characterization





#### SPACE LEVEL COMPONENTS, MODULES & SUBSYSTEMS

#### Class S Screening & Qualification

- VI to Methods 2010A & 2017K
- Temp Cycle Stress Test
- High Temp Burn-In & Life Test
- Wafer Lot Acceptance Test
   Bond Pull & Die Shear Test
   SEM Inspection
   Metal & Glass Thicknesses
- Serialized Test Data
- Qualification Report

- Class S screening on standard & custom product die and SMT packaging.
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FET Channel SEM



Serialized Die in GEL-PAK



Hermetic SMT Package



**Hermetic Modules** 



Chip (Die)

## DESIGNER'S KITS



#### **Evaluation Boards & ICs Reduce Design Cycle Time**

#### 7 DESIGNER'S KITS AVAILABLE TO CHOOSE FROM!



- ♦ Gain Blocks DC 6 GHz, HMC-DK001
- ♦ Linear Driver Amplifiers 0.4 2.5 GHz, HMC-DK002
- ♦ High IP3 Mixers 0.45 4.0 GHz, HMC-DK003
- ♦ Digital Attenuators DC 6 GHz, HMC-DK004
- ♦ SPDT Switches DC 12 GHz, HMC-DK005
- ♦ Passive Attenuator Chips DC 50 GHz, HMC-DK006
- ♦ Serial/Parallel USB Interface Kit, HMC-DK008

Design engineers can order pre-packaged MMIC Designer's Kits which enable them to quickly assess which Hittite product is the best choice for their application. The end result is a design that goes to layout more quickly and with fewer subsequent changes.

Each Hittite Designer's Kit contains an assembled & tested connectorized evaluation board, 5 to 10 ICs of each part and the latest Hittite CD-ROM catalog.

Designer's Kit		!	Kit Contents	
Designer's Kit	IC	s	Eva	l Boards
Gain Blocks DC - 6 GHz HMC-DK001	HMC474MP86E HMC476MP86E HMC313E HMC311ST89E HMC478MP86E HMC478ST89E	HMC479MP86E HMC479ST89E HMC481ST89E HMC480ST89E HMC481MP86E HMC482ST89E	104217 – HMC313E 110161 – HMC478ST89E 107490 – HMC481MP86E	
Linear Driver Amps 0.4 - 2.5 GHz HMC-DK002	HMC454ST89E HMC450QS16GE HMC413QS16GE	HMC452ST89E HMC453ST89E HMC457QS16GE	107749 – HMC454ST89E 108349 – HMC450QS16GE 105000 – HMC413QS16GE	108712 - HMC452ST89E 108718 - HMC453ST89E 106043 - HMC457QS16GE
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Serial/Parallel USB Interface Kit HMC-DK008	The HMC-DK008 Serial/Pa attenuators, interface and		s kit enables users to interface v	vith Hittite's family of digital
EKIT01-HMC6383	Programmable Direct Conflexibility and industry lead		000 MHz. Hittite's HMC6383 fe	atures unparalleled receiver



## PACKAGE INFORMATION

#### **Available Plastic, Ceramic, Hermetic SMT & Connectorized Module Packages**





38.10 x 33.53 x 5.84 mm

E or √=RoHS Compliant.

For more information on our "Green" component program, please contact <a href="mailto:earthfriendly@hittite.com">earthfriendly@hittite.com</a> for details on our RoHS Compliant products or see the RoHS Compliant Components link on our web site.

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